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AN OSCILLATOR WITH SWITCHED REACTIVE ELEMENTS

5 The invention relates to an arrangement for generating a clock signal.

Digital video signal processing systems with features such as on-screen display of text and picture-in-picture for both television receiver and video tape recorder signal sources may
 10 require a clock signal that is phase locked to a horizontal synchronization signal, referred to as line-locked clock. It may be advantageous to form a phase-locked loop (PLL) system for line-locked clock generation for use as a building block in large scale CMOS video signal processing integrated circuits. In such PLL, it
 15 may be desirable to have, for example, a clock frequency that ranges from 25 MHz to 40 MHz with a jitter that is less than 2nS. For such PLL it may be desirable to utilize only one pin for off-chip components. It may also be desirable to use the PLL system with each of the NTSC, PAL and SECAM systems.

20 It may further be advantageous to operate the PLL with input sync signal encountered in low-cost consumer video tape recorders without time-base correction where the horizontal sync can periodically make large phase changes such that the clock signal tracks such sync signal. It may be further desirable
 25 to rapidly reduce phase and frequency errors and minimize overshoot and jitter as the PLL settles into phase lock. In addition, it may be desirable to have the PLL discriminate between true output clock phase/frequency errors and those arising from contamination of the input horizontal sync signal
 30 with noise bursts or occasional missing pulses.

A PLL system, embodying an inventive feature, utilizes both digital and analog control of an R-C Voltage-Controlled Oscillator to acquire and maintain phase lock of an output clock with respect to an input horizontal sync signal.
 35 Depending on the magnitude and consistency of the output clock phase and frequency error, the system automatically selects one

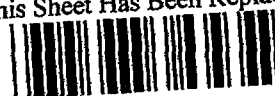
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of, for example, five control modes of operation of varying
5 sensitivity. The control modes of operation are such that large errors result in large, coarse corrective actions, and small errors result in small, or fine corrective actions.

In a PLL, embodying a different inventive feature, a frequency of an output signal of an oscillator is controlled in
10 accordance with switched capacitors that are selectively coupled to a positive feedback path of the oscillator. A given group of switched capacitors selects a corresponding frequency range portion selected from an entire range of frequencies of the oscillator output signal. By varying the selection of the switched
15 capacitors, the frequency range portion of the frequencies of the oscillator varies. Within the given frequency range portion, the frequency of the oscillator output signal is controllable by a control signal without varying the selection of the switched capacitors. The control signal can vary the oscillator frequency
20 only within a limited portion of the entire range of frequencies. Therefore, stability and noise immunity is increased. Advantageously, jitter of the output signal of the oscillator is also reduced. Consequently, the oscillator can be realized with capacitors that can be fabricated within an integrated circuit. The
25 integrated circuit may also include the remaining active circuit elements of the oscillator. When a large frequency error occurs between the horizontal synchronization signal and an output signal of the oscillator, the PLL operates in a coarse frequency correction mode.

30 In accordance with a further inventive feature, in each capacitor switching step that occurs in a sequential manner, a predetermined pair of the switched capacitors are either both coupled to the positive feedback path or both decoupled from the positive feedback path, in accordance with the direction of the
35 frequency error. The frequency of the oscillator output signal changes progressively in the same direction, or monotoneously, in



each switching step in the sequence of steps until the frequency error changes direction. When the frequency error changes direction, operation in the coarse frequency correction mode ceases and any remaining frequency error is relatively small. Advantageously, monotonically changing the frequency of the oscillator output signal simplifies the control of the PLL because in each step the direction of the change of the frequency is not dependent on tolerances of, for example, the capacitors.

An apparatus, embodying an additional inventive feature, for generating an oscillatory signal that is locked to an input signal, includes an amplifier. A plurality of switched reactive elements selectively coupled in a positive feedback path formed between an output and an input of the amplifier are provided. The oscillatory signal has a frequency that is selected from a corresponding portion of a range of frequencies in accordance with a selection of the switched reactive elements. A frequency error is measured between the oscillatory and input signals. A first switching control signal that is coupled to a switching arrangement associated with the switched reactive elements is generated to select the switched reactive elements in accordance with the frequency error. When the frequency error exceeds a first value, the selection of the switched reactive element varies in switching steps of a coarse frequency correction mode of operation to reduce the frequency error progressively in successive switching step. A second control signal that is coupled to a control input of the amplifier is generated for varying the frequency of the oscillatory signal within the corresponding portion of the range. The frequency error is corrected in a fine error correction mode of operation when the frequency error does not exceed the first value, without varying the selection of the switched reactive elements.

FIGURE 1 illustrates a block diagram of a phase-lock-loop (PLL), embodying an aspect of the invention;



FIGURES 2A, 2B and 2C illustrate a detailed schematic diagram of a programmable switched R-C voltage controlled oscillator of the PLL of FIGURE 1;

FIGURE 3 illustrates a switched capacitor arrangement of the oscillator of FIGURES 2A-2C;

FIGURE 4 illustrates waveforms useful for explaining the arrangement of FIGURES 2A-2C;

FIGURE 5 illustrates a flow chart useful for explaining the operation of the PLL of FIGURE 1;

FIGURES 6, 7A and 7B illustrate more detailed diagrams of portions of the PLL of FIGURE 1;

FIGURE 8 is a table useful for explaining the operation of a decoder of FIGURE 1;

FIGURES 9a-9c are waveforms useful for explaining the operation of the PLL of FIGURE 1;

FIGURE 10 illustrates a schematic of a charge pump stage of the PLL of FIGURE 1;

FIGURE 11 illustrates a detailed schematic of a phase detector of the PLL of FIGURE 1;

FIGURES 12a-12g illustrate waveforms useful for explaining the operation of the phase detector of FIGURE 11; and

FIGURES 13a-13d illustrate waveforms useful for explaining the operation of the charge pump stage of the PLL of FIGURE 1.

FIGURE 1 illustrates a block diagram of a phase-lock loop circuit (PLL) 100, embodying an aspect of the invention. A base band video signal VIDEO-IN obtained from, for example, a video detector, not shown, of a television receiver is coupled to a conventional sync separator 50 that generates pulses of a horizontal sync signal HSRef having a period H at a horizontal deflection frequency f_H that is in, for example, the NTSC standard 15,734 Hz.

An oscillatory signal ClkDiv is produced at an output of
 5 a programmable divide-by-N counter 52 by frequency dividing an
 output signal Clk of PLL 100 produced in a programmable,
 resistor-capacitor (R-C) type voltage-controlled-oscillator (RCVCO)
 53. Output signal Clk may be used in various stages, not shown, of
 the television receiver for video signal processing. In steady state
 10 operation, the frequency of signal Clk is equal to $N \times f_H$. The value
 N denotes a ratio between the frequency of signal Clk and that of
 signal ClkDiv. The value N that is selectable in the range of 750-
 2600 is provided by a constant digital word signal Nset that is
 coupled to counter 52 for presetting counter 52 once in each
 15 period of signal ClkDiv.

FIGURES 2A, 2B and 2C illustrate a schematic diagram
 of RCVCO 53 of FIGURE 1. Similar symbols and numerals in
 FIGURES 1 and 2A-2C indicate similar items or functions. RCVCO
 53 of FIGURE 2B includes a differential amplifier 531 formed by a
 20 pair of transistors MP9 and MP10. A current source transistor
 MP8 produces a corresponding source electrode current in each of
 transistors MP9 and MP10. Amplifier 531 includes load resistors
 R5 and R6 of transistors MP9 and MP10, respectively. Similarly, a
 differential amplifier 532 of FIGURE 2C is formed by transistors
 25 MP11, MP12 and MP13 and load resistors R7 and R8. A pair of
 signals X2a and X1a developed in load resistors R5 and R6 of
 amplifier 531 are coupled to gate electrodes of transistors MP12
 and MP13 via a pair of R-C delay networks 533a and 533b,
 respectively, that produce nominally the same phase shift. The
 30 phase shift produced by network 533a or 533b is controllable in a
 coarse frequency correction mode of operation, as explained later
 on. The phase shift determines, in part, the frequency of
 oscillation of signal Clk.

Delay network 533a includes a resistor R1A and a
 35 non-switched capacitor C1A. A switched capacitor bank SWA(0) is
 also coupled to capacitor C1A. A delayed signal TA(0) is



developed at a junction terminal TA(0)a, between capacitor C1A
 5 and resistor R1A. Signal TA(0) is coupled via a resistor R2A to a
 capacitor C2A. A switched capacitor bank SWA(1) is also coupled
 to capacitor C2A. A delayed signal TA(1) is developed in capacitor
 C2A. Signal TA(1) is delayed with respect to signal TA(0).

Similarly, network 533b includes a resistor R1B, a capacitor C1B
 10 and a bank SWB(0) that produces a signal TB(0). Network 533b
 includes a resistor R2B, a capacitor C2B and a bank SWB(1) that
 produces a signal TB(1).

A pair of signals Y1 and Y2 of FIGURE 2C developed in
 load resistors R7 and R8, respectively, of amplifier 532 are
 15 coupled via R-C delay networks 534b and 534a, respectively, that
 produce nominally the same phase shift. Networks 534a and
 534b operate in a similar manner to networks 533a and 533b.
 Network 534a includes a resistor R3A, a capacitor C3A and a bank
 SWA(2) that produces a delayed signal TA(2). Signal TA(2) is
 20 coupled via a resistor R4A to a capacitor C4A and to a bank
 SWA(3) that produces a delayed signal TA(3). Signal TA(3) is
 further delayed via a resistor R5A and a capacitor C5A to produce
 a further delayed signal TA(4). Similarly, delay network 534b
 includes resistors R3B, R4B and R5B that are analogous to resistors
 25 R3A, R4A and R5A, respectively, and capacitors C3B, C4B and C5B
 that are analogous to capacitors C3A, C4A and C5A, respectively.
 Network 534b produces delayed signals TB(2), TB(3) and TB(4)
 that are analogous to signals TA(2), TA(3) and TA(4), respectively.

Signals TB(3) and TA(3) are coupled to gate electrodes
 30 of a pair of transistors MP3 and MP2, respectively, of an analog
 multiplier 535 of FIGURE 2A. Similarly, signals TB(4) and TA(4),
 that are delayed with respect to signals TB(3) and TA(3),
 respectively, are coupled to gate electrodes of a pair of transistors
 MP7 and MP6, respectively, of multiplier 535 of FIGURE 2A.

35 In multiplier 535, transistors MP2 and MP3 form a
 differential amplifier 535a having a controllable gain. Similarly,



transistor MP6 and MP7 form a differential amplifier 535b having
5 a controllable gain. The gains of amplifiers 535a and 535b vary in
opposite directions in accordance with variations in drain currents
produced by a pair of transistors MP1 and MP5 that form a
differential amplifier 535c. The drain currents in transistors MP1
and MP2 vary in opposite directions in accordance with a voltage
10 difference between gate electrodes of transistors MP1 and MP5.

A constant DC reference voltage VREF is developed at
the gate of transistor MP1. A control, output signal VCOCV
produced in a charge pump control stage 54 of FIGURE 1 is
developed at the gate of transistor MP5 of FIGURE 2A to control
15 the frequency/phase of signal Clk, in a fine error correction mode
of operation, as explained later on.

The drain electrode of transistor MP2 is coupled to the
drain electrode of transistor MP6 to develop a sum signal X1.
Signal X1 is developed in a pair of parallel coupled load resistors
20 R10 and R12 and is coupled to the gate electrode of transistor
MP10 of amplifier 531 of FIGURE 2B. Similarly, the drain
electrode of transistors MP3 of FIGURE 2A is coupled to the drain
electrode of transistor MP7 to develop a sum signal X2. Signal X2
is developed in a pair of load resistors R11 and R13 and is coupled
25 to the gate electrode of transistor MP9 of amplifier 531 of FIGURE
2B.

The signal gain, for example, via transistor MP2 varies
in the opposite way to that via transistor MP6. The phase shift of
signal X1 is determined by the vectorial sum of a pair of signals
30 having a phase difference therebetween produced from the drain
currents in transistors MP2 and MP6, respectively. Thus, the
phase shift of signal X1 varies in a fine or gradual manner when
analog signal VCOCV that is coupled to amplifier 535c varies in a
gradual manner. Similarly, the phase shift of signal X2 also varies
35 in a fine or gradual manner in accordance with signal VCOCV.
Signal X1 is nominally at an opposite phase with respect to signal

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5 X2. Varying the phase shift of signal X1 or X2 causes the
oscillation frequency of RCVCO 53 and of signal Clk to vary, as
explained later on.

10 It may be desirable to achieve a wide frequency range
of, for example, 25-40 MHz of signal Clk and also to compensate
for tolerances, temperature variations and for aging in the R-C
delay networks. The R-C delay networks are formed in RCVCO 53
using integrating circuit fabrication technique.

15 The frequency of RCVCO 53 can be stepped up or down
in a coarse frequency correction mode of operation. For example,
the coarse frequency correction mode may occur immediately
after power is applied. To provide the coarse frequency
correction mode, the aforementioned four switch-capacitor banks,
SWA(i), are provided. The parameter "i" that designates the
switch-capacitor bank assumes the four values, 0 to 3. Switch-
capacitor banks SWA(i) are coupled to four corresponding
20 terminals where signals TA(i), referred to before, are developed.
Thus, a given bank SWA(i) is coupled to a corresponding terminal
where signal TA(i) is designated by the same value "i". Similarly,
the afore-mentioned four switch-capacitor banks, SWB(i), are
coupled to corresponding four terminals where signal TB(i),
25 referred to before, are developed. In the same way, the
parameter "i" assumes the values 0 to 3.

Each bank SWA(i), such as bank SWA(0) of FIGURE 2B,
includes eight parallel coupled switch-capacitor arrangements. A
given switch-capacitor arrangement of a given bank SWA(i) is
30 formed by a transistor switch SA(4j+i), shown in FIGURE 3, that is
coupled in series with a corresponding capacitor CA(4j+i). Similar
symbols and numerals in FIGURES 1, 2A-2C and 3 indicate similar
items or functions. For a given bank SWA(i) of FIGURES 2B and
2C, the parameter j assumes, selectively, one of the eight values 0
35 to 7.



A given transistor switch $SA(4j+i)$ of FIGURE 3 is
 5 coupled in series with a corresponding capacitor $CA(4j+i)$ such that
 the value of "i" is common to both switch $SA(4j+i)$ and to capacitor
 $C(4j+i)$ and the value of "j" is also common for both. Similarly,
 each bank $SWB(i)$ of FIGURES 2B and 2C includes eight parallel
 coupled transistor switch-capacitor arrangements, such as, for
 10 example, bank SWA . Each of such eight arrangements is formed
 by a transistor switch $SB(4j+i)$ of FIGURE 3 that is coupled in series
 with a capacitor $CB(4j+i)$.

In each pair of banks, $SWA(i)$ and $SWB(i)$, of FIGURES
 2B and 2C designated by a common value "i", such as, for example,
 15 banks $SWA(0)$ and $SWB(0)$, eight control signals $CF(4j+i)$ control
 the corresponding eight pairs of transistor switches $SA(4j+i)$ and
 $SB(4j+i)$ designated also by the common value of "i" and the
 common value of "j". Signals $CF(4j+i)$ are developed in a manner
 that is described later on. Thus, the total of 32 pairs of switches
 20 $SA(4j+i)$ and $SB(4j+i)$ are controlled by the 32 control signals
 $CF(4j+i)$, respectively. The value of "i" for a given pair of switches
 $SA(4j+i)$ of FIGURE 3 and $SB(4j+i)$ and for control signal $CF(4j+i)$
 that controls such pair of switches is the same. The value of "j" is
 also common for the given pair of switches $SA(4j+i)$ and $SB(4j+i)$
 25 and for control signal $CF(4j+i)$ that controls such pair.

When a given control signal $CF(4j+i)$ assumes a TRUE
 state, a corresponding capacitor $CA(4j+i)$ of the corresponding
 bank $SWA(i)$ and a corresponding capacitor $CB(4j+i)$ of the
 corresponding bank $SWB(i)$ are switched in or coupled via a pair
 30 of the switches $SA(4j+i)$ and $SB(4j+i)$ to the terminals where signals
 $TA(i)$ and $TB(i)$, respectively, are developed. Thereby, an increase
 phase delay and a corresponding decrease in the oscillation
 frequency of signal Clk of FIGURE 2C occur. On the other hand,
 when a given control signal $CF(4j+i)$ of FIGURE 3 assumes a FALSE
 35 state, the corresponding pair of capacitors are switched out or

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5 decoupled, causing an increase in the oscillation frequency of signal Clk of FIGURE 2C.

A current mirror reference circuit 537 of FIGURE 2A includes a PMOS transistor MP20 that provides a small start-up current such as 1 μ A. The start-up current causes a voltage level at a terminal NB to initially rise to a threshold voltage of a
10 transistor MN10, typically 0.8V. Voltages at a terminal NR and at terminal NB are compared in a balanced PMOS current mirror amplifier formed by transistors MP23, MP24, MN13 and MN14.

Negative feedback from a terminal NF is applied to the gate of a transistor MN12 forcing the voltages at terminals NR and
15 NB to be equal. The current flowing in a resistor R1 is, therefore, proportional to the voltage at terminal NB. Once current starts flowing in resistor R1, in transistor MN12 and in transistor MP22, additional current is sourced into terminal NB which causes the voltage at terminal NB to rise to a level of about 1.5V. Thus, a
20 reference current flowing in transistor MP22 is nominally 0.25 mA.

An output voltage CS1 of current mirror reference circuit 537 developed at the drain of transistor MP22 is coupled to the gates of transistors MP4 and MP8 of FIGURE 2B and transistor
25 MP11 of FIGURE 2C. As a result, the current flowing in transistor MP4 of FIGURE 2A is nominally 3 mA and the current flowing in each of the amplifiers sourced by transistors MP8 and MP11 is 1.5 mA. Circuit 537 of FIGURE 2A maintains stability of the frequency of the oscillator with respect to supply voltage change.
30 Simulation shows that sensitivity to supply voltage change is 0.9%/V and to temperature change is -0.012%/°C.

RCVCO 53 of FIGURES 2A-2C is constructed in a differential symmetrical manner. Signals X2, Y1, TA(0), TA(1), TB(2), TB(3) and TB(4), defining a first positive feedback path, are
35 differentially symmetrical with respect to signals X1, Y2, TB(0), TB(1), TA(2), TA(3) and TA(4), respectively, defining a second

positive feedback signal path. Therefore, phase difference
5 between a pair of differentially symmetrical signals such as, for
example, signals Y1 and Y2 does not vary when the gain of, for
example, amplifiers 535a and 535b of FIGURE 2A varies or when
a temperature variation occurs. RCVCO 53 oscillates at a
frequency which is determined by the total phase shift in its pair
10 positive feedback paths.

In accordance with an inventive feature, as explained
before, a pair of capacitors CA(4j+i) and CB(4j+i) of FIGURES 2A-2C
are switched in together or switched out together. Therefore,
advantageously, the differential symmetrical configuration is not
15 disturbed in each step of the coarse frequency error correction
mode.

FIGURE 4 illustrates an example of simulated
waveforms of signals Y1 and Y2 of FIGURE 1 when all the
switched capacitors in RCVCO 53 are decoupled by signals CF(4j+i),
20 resulting in maximum frequency or minimum period of signal Clk
such as 19.62nS. Similar symbols and numerals in FIGURES 1, 2A-
2C, 3 and 4 indicate similar items or functions.

As shown in FIGURE 4, signals Y1 and Y2 are nearly
identical in magnitude and they are phased by 180 degrees with
25 respect to each other. Signals Y1 and Y2 are differentially
symmetrical signals because of the differential symmetrical
configuration. Thus, crossover points in signals Y1 and Y2, such as
points CO, that occur when the instantaneous values of signals Y1
and Y2 are simultaneously the same, occur at the opposite phase.
30 Advantageously, the crossover points CO are nearly equally
spaced in time as a result of the aforementioned differential
symmetrical configuration. Because of the symmetrical
configuration, the duty cycle of signal Clk is, advantageously, not
affected by gain variations and temperature caused component
35 variations. Therefore, advantageously, a relatively simple
differential-to-single ended translation circuit 536 of FIGURE 2C

that receives signals Y1 and Y2 and is formed by transistors
 5 MP15, MP16, MN20 and MN21 and gates U1 and U2 generates
 signal Clk at approximately 50% duty cycle. Furthermore, the
 differential symmetry configuration provides improved common
 mode noise rejection.

The measured noise bandwidth of RCVCO 53 is -30dB
 10 at 350 Hz. The short term stability of RCVCO 53 within 1 second is
 about ± 150 Hz or 20 ppm, corresponding to a 1.3 ns jitter in one
 horizontal line period H of 63.5 μ sec.

To control the frequency of RCVCO 53, sync signal
 HSRef of FIGURE 1 is coupled to a frequency detector and control
 15 stage 55. FIGURE 5 illustrates a flow chart useful for explaining
 the operation of PLL 100 of FIGURE 1. FIGURES 6, 7A and 7B
 illustrate corresponding portions of stage 55 of FIGURE 1 in more
 detailed block diagram. Similar symbols and numerals in FIGURES
 1, 2A-2C, 3-6, 7A and 7B indicate similar items or functions.

20 In the portion of stage 55 that is shown in FIGURE 6,
 signal HSRef is coupled to an input terminal Clear/Enable of a 13-
 bit-counter 56. Signal Clk of RCVCO 53 of FIGURE 1 is coupled to
 an input terminal CLOCK of counter 56 of FIGURE 6. FIGURES 9a
 and 9b illustrate an example of the pulses of signals ClkDiv and
 25 HSRef, respectively, of FIGURE 6. Similar symbols and numerals in
 FIGURES 1, 2A-2C, 3-6, 7A, 7B and 9A-9C indicate similar items or
 functions.

Counter 56 of FIGURE 6 counts pulses of signal Clk that
 occur during a given period H and referred to as an interval
 30 MEASUREMENT in FIGURE 9b. At the end of interval
 MEASUREMENT, counter 56 of FIGURE 6 contains a binary word
 signal NCL. Signal NCL has a numerical value that is equal to the
 number of clock pulses or periods of signal Clk that occur during a
 given period of signal HSRef. Thus, signal NCL contains the ratio
 35 between the frequency of signal Clk and that of signal HSRef.



Signal NCL is coupled to a subtractor 65 that generates
 5 a binary word signal Nerr by forming a difference between the
 value of signal NSET and that of signal NCL. Signal NSET is a
 constant binary word that is equal to the ratio between the
 frequency of signal Clk and that of signal ClkDiv, as indicated
 before. Signal Nerr is stored in a latch 57 when a timing control
 10 signal CLKH occurs. Signal CLKH occurs immediately following that
 period H of signal HSRef during which signal Nerr is measured and
 generated.

Stored signal Nerr is read out at an output of latch 57
 as an output signal NERR. Error signal NERR has a value that is
 15 equal to a difference between the number of clock periods of
 signal Clk that occur during the given period MEASUREMENT of
 signal HSRef of FIGURE 9b and the number of clock periods of
 signal Clk of FIGURE 6 that occur during the period of signal ClkDiv
 of FIGURE 9a. Such difference is zero and represents no error, for
 20 example, when PLL 100 of FIGURE 1 is in a phase-lock condition.
 Thus, signal NERR is indicative of a cycle related or frequency
 error. The measurement operation in which signal NERR is
 developed is depicted in a flowchart path 197 of the flow chart of
 FIGURE 5.

Frequency error indicative signal NERR of FIGURE 6 is
 coupled to an input of an absolute value forming stage 58 of
 FIGURE 7A that produces a binary word signal $|Nerr|$. Signal
 $|Nerr|$ is equal to the absolute value of signal NERR. Signal $|Nerr|$
 is compared in a comparator 59 with a constant value word signal
 30 THRESHOLD_1 that is equal to 8% of the magnitude of word signal
 NSET. The desired period length of signal ClkDiv is contained in
 word signal NSET. Comparator 59 generates a word signal 59a
 when the error in the length of the period of signal ClkDiv, as
 measured by the number of clock cycles of signal Clk, is greater
 35 than 8% of the desired period length of signal ClkDiv.

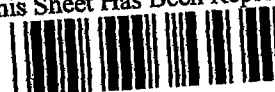


Signal 59a is coupled to a reset input terminal RESET
 5 of a 6-bit counter 61 that counts up once in each period of clock
 signal ClkDiv, when counting is enabled in counter 61. Counter 61
 produces a signal 61a, the most-significant-bit MSB of counter 61.
 Counting is enabled in counter 61 when signal 59a is generated.

Signal 61a is coupled via an OR gate 62 to a "J" input
 10 terminal of a flip-flop 63. A TRUE state of an output signal CFR of
 flip-flop 63 is obtained should, in each of the 32 immediately
 preceding periods H of signal ClkDiv, the error in the length of the
 period of signal ClkDiv, as provided by the value of signal $|Nerr|$,
 be greater than 8% of the desired period length.

As long as such 32 periods H of signal ClkDiv of FIGURE
 15 9a have not elapsed, RCVCO 53 of FIGURE 1 is not affected,
 referred to as an idle mode operation and depicted in a path 194
 of the flow chart of FIGURE 5. Advantageously, the idle mode
 occurs in a manner to prevents the occurrence of the coarse
 20 frequency correction mode, for example, throughout a vertical
 blanking interval (VBI). During the vertical blanking interval,
 equalizing pulses EP of FIGURE 1 occur. Pulses EP have a period
 that is one-half of period H. Therefore, equalizing pulses EP in
 signal HSRef of FIGURE 1 produce a value of error signal $|Nerr|$ of
 25 FIGURE 7A that is greater than 8% of the desired period length.
 However, because the number of equalization pulses EP of FIGURE
 1 is smaller than 32, counter 61 and "OR" gate 62 of FIGURE 7A
 prevent signal CFR from attaining the TRUE state, throughout the
 vertical blanking interval. Therefore, operation in the coarse
 30 frequency correction mode is prevented. As a result of the
 operation in the idle mode, advantageously, the phase of RCVCO
 53 is not disturbed throughout the vertical blanking or retrace
 interval.

Assume that the number of periods of signal ClkDiv in
 35 which error signal $|Nerr|$ is greater than 8% of the desired period
 length exceeds 32. This situation is indicative of a large frequency



error not due to operation in the vertical blanking interval.

5 Therefore, signal CFR of flip-flop 63 of FIGURE 7A would be generated at the TRUE state. When signal CFR is generated, it causes PLL 100 of FIGURE 1 to operate in the coarse frequency error correction mode of operation. During operation in the coarse frequency error correction mode, coarse frequency error is
10 reduced sequentially in RCVCO 53 in switching steps. The way signal CFR is generated is indicated in flow chart paths 197, 200, 201, 196 and 199 of the flow chart in FIGURE 5.

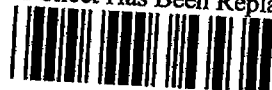
FIGURE 10 illustrates a more detailed diagram of charge pump stage 54 of FIGURE 1. Similar symbols and numerals
15 in FIGURES 1, 2A-2C, 3-6, 7A, 7B, 9a-9c and 10 indicate similar items or functions. The table in FIGURE 10 provides the direction of signal flow and the state of the switches in stage 54.

Throughout the coarse frequency error correction mode, charge pump stage 54 of FIGURE 10 produces analog control signal VCOCV
20 of RCVCO 53 of FIGURE 2A at a constant level that is equal to reference voltage VREF, provided via a switch SW1 of FIGURE 10. Signal VCOCV of FIGURE 10 is established approximately at its middle voltage variation range.

In the coarse frequency error correction mode, a 5-bit
25 binary counter 66 of FIGURE 6 counts up or down alternate pulses of signal ClkDiv. The direction of counting in counter 66, up or down, is determined in accordance with the state of a most significant or a sign bit SIGN of word signal NERR. A 5-bit output word signal CFRL(4:0) of counter 66 is coupled to an input of a
30 decoder 64, referred to herein as a "thermometer" decoder. Thermometer decoder 64 produces the aforementioned 32 separate control signals CF(4j+i) by decoding the 5-bit signal CFRL(4:0).

The table of FIGURE 8 shows those of signals CF(4j+i) of
35 FIGURES 2A, 2B and 8 that are at the TRUE state and those that are at the FALSE state for each value of 5-bit word signal

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CFRL(4:0) of FIGURES 6 and 8. In the table of FIGURE 8, binary "1" represents the TRUE state and binary "0" represents the FALSE state. As shown in FIGURE 8, when counter 66 of FIGURE 6 counts up, only one of control signals CF(4j+i) of FIGURE 8 changes state. The change in state is from FALSE to TRUE state. Similarly, when counter 66 of FIGURE 6 counts down, only one of control signals CF(4j+i) of FIGURE 8 changes state; whereas, the change in state is from TRUE to FALSE.

In the coarse frequency error correction mode, a measure/control sequencer unit 67 of FIGURE 6 generates a signal CFR_Enable that enables counter 66 to count up/down alternate pulses of signal ClkDiv. Alternate pulses of signal ClkDiv occur in alternate periods H of signal HSRef. Only during intervals CONTROL, that occur in alternate periods of signal HSRef of FIGURE 9b, between intervals MEASUREMENT, signal CFR_Enable enables counter 66 of FIGURE 6 to change states. During the other alternate periods of signal HSRef of FIGURE 9b, when intervals MEASUREMENT occur, the value of signal NCL is measured, as explained before, but counter 66 of FIGURE 6 does not change states. Counter 66 does not change states while signals NERR or NCL of FIGURE 9b are being measured. By preventing counter 66 of FIGURE 6 from changing states, during a given interval MEASUREMENT of FIGURE 9b, the frequency of RCVCO 53 of FIGURE 1 does not change at the same time that the frequency of RCVCO 53 is being measured. Thus, a given switching step in the coarse frequency correction mode requires two horizontal clock pulses of signal ClkDiv and occurs every pair of periods H. As a result of not having the frequency of RCVCO 53 changed when it is being measured, a more stable and precise frequency control operation is obtained.

For explanation purposes of the coarse frequency error correction mode, assume that, in a given interval MEASUREMENT of FIGURES 9a and 9b, denoted as interval 602, the measured



frequency of signal Clk of RCVCO 53 of FIGURES 2A-2C is higher
 5 than required. Such situation is indicated by the occurrence of a
 positive value of signal NERR of FIGURE 6. Consequently, at the
 end of the immediately following interval CONTROL of FIGURES 9a
 and 9b, denoted as interval 603, counter 66 of FIGURE 6 is
 incremented. The result is that a corresponding pair of capacitors
 10 CA(4j+i) and CB(4j+i) of FIGURES 2A, 2B and 2C are switched-in, in
 accordance with updated incremented value of word signal
 CFRL(4:0) of FIGURE 6. The updated value of signal CFRL(4:0) is
 incremented or decremented in accordance with the sign bit SIGN
 of signal NERR of FIGURE 6. Because additional pair of capacitors
 15 is coupled to the positive feedback paths, a decrease in the
 frequency of signal Clk occurs. On the other hand, if the
 frequency of signal Clk is lower than required, a pair of capacitors
 CA(4j+i) and CB(4j+i) of FIGURES 2B or 2C would be switched out
 or decoupled from the positive feedback paths. The capacitor
 20 switching occurs in the immediately following interval CONTROL,
 or interval 603, of FIGURES 9a and 9b, causing an increase in the
 frequency of RCVCO 53 of FIGURES 2A-2C.

Thermoter decoder 64 of FIGURE 6 operates in such a
 way that a change of state in counter 66 causes only one pair of
 25 switched capacitors in the corresponding pair of positive feedback
 paths, respectively, to be switched in or out and no other pair of
 capacitors is affected, as explained before. Therefore,
 advantageously, the change, increase or decrease, in the frequency
 of signal Clk of FIGURE 2C is monotonical and not affected by
 30 component tolerances. Thus, for the entire frequency range, the
 frequency of signal Clk is proportional to the value of word signal
 CFRL(4:0) of FIGURE 6.

For explanation purpose, assume that prior to the end
 of a given interval CONTROL, denoted as an interval 601, of
 35 FIGURES 9a and 9b, the value of signal CFRL(4:0) of FIGURE 6 is
 equal to 23. The value 23 corresponds to $j=5$ and $i=3$, since

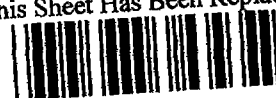
4j+i=23. As explained before, i is selected only from the values 0
5 to 3 and, j is selected only from the values 0 to 7.

Further assume that the sign bit SIGN of signal NERR is such that counter 66 of FIGURE 6 counts up, at the end of interval 601. Thus, in a subsequent interval MEASUREMENT, denoted as an interval 602 of FIGURES 9a and 9b, signal CFRL(4:0) of FIGURE
10 6 contains an incremental value that is equal to 24, corresponding to j=6 and i=0 since 4j+i=24. Only capacitors CA(24) and CB(24) in banks SWA(0) and SWB(0), respectively, of FIGURE 2 will be switched in and coupled to the corresponding pair of positive feedback paths in RCVCO 53 at the end of interval 601 of FIGURES
15 9a and 9b. The switched capacitors that were already coupled to the corresponding positive feedback paths, prior to the end of interval 601 of FIGURES 9a and 9b, will not be affected by the increment of the value of signal CFRL(4:0) of FIGURE 8. In this way, capacitors CA(4j+i) and CB(4j+i) of FIGURES 2B and 2C are
20 switched in or out in a progressive or monotonical manner.

In each interval CONTROL of FIGURE 9b, the change in the frequency of RCVCO 53 of FIGURES 2A-2C is approximately 4% of the entire range of operating frequencies of RCVCO 53. Thus, the entire frequency range of RCVCO 53 can be sequenced in 32
25 capacitor switching steps or fewer.

Sign bit SIGN of signal NERR of FIGURE 7A is coupled, both delayed and undelayed, to a pair of input terminals of an exclusive or gate 69. The delayed sign bit is produced in a latch 68. Gate 69 produces an output signal 69a that is coupled to a "K"
30 input terminal of J-K flip-flop 63.

In carrying out an inventive feature, switched capacitors CA(4j+i) and CB(4j+i) are switched in or switched out of the positive feedback path in steps of a negative feedback loop. The generation of signal CFR is disabled and operation in the
35 coarse frequency error control mode ceases when the difference between the measured and expected lengths of the period of



5 signal ClkDiv, as determined by the sign bit SIGN of signal NERR, changes sign. The sign change of signal NERR is indicative of attaining a frequency error that is smaller or equal to 4% of the entire frequency range. Thereafter, counter 66 of FIGURE 6 ceases to change states and the last state of signals CFRL (4:0) and CF (4j+i) remains unchanged.

10 Signal NERR of FIGURE 7B is coupled to a first input A of a subtractor 70. Signal NERR, delayed via a latch 71 by one period of signal ClkDiv, is coupled to a second input B of subtractor 70. An absolute value of a difference between the input signals of subtractor 70 is obtained in an absolute value forming stage 72
15 and is compared in a comparator 73 against a value contained in a digital word signal THRESHOLD_2.

Assume that the period length error of signal ClkDiv changes, from a given period H to the immediately following one of signal ClkDiv, by less than 2% of the expected period length of clock signal ClkDiv. The 2% threshold value is contained in signal THRESHOLD_2. Therefore, a signal CONSISTENCY is generated in an output 73a of comparator 73. Thus, signal CONSISTENCY is generated when the magnitude of signal NERR varies by no more than 2% of the value of signal NSET of FIGURE 6 from one clock
20 period H to the immediately following one of signal ClkDiv. It follows that signal CONSISTENCY of FIGURE 7B is indicative of the presence of a stable and noise free synchronizing signal HSRef and error signal Nerr.

Signal |Nerr| of FIGURE 7A is compared with a
30 constant value that is equal to 2 in a comparator 60. Comparator 60 generates a signal 60a when the error or difference in the period length of signal ClkDiv with respect to that of signal HSRef is smaller than 2 clock periods of signal Clk.

Assume that all of the followings occur: signal
35 CONSISTENCY of FIGURE 7A is produced, the value of signal |Nerr| is greater than or equal to 2, but smaller than 8% of the value of



5 signal Nset, as provided in signal 60a of FIGURE 7A and signal CFR
 is not generated. Therefore, an "AND" gate 74 produces a signal
 FFR. Signal FFR initiates and establishes a fine or gradual
 frequency error correction mode of operation in which the state of
 coupling or decoupling of the switched capacitor in FIGURES 2A-2C
 is not affected. Flow chart paths 202, 203, 204 and 205 in the
 10 flow chart of FIGURE 5 depict the conditions for the generation of
 signal FFR of FIGURE 7A. On the other hand, should signal
 CONSISTENCY not be generated, RCVCO 53 of FIGURE 1 will not be
 affected, resulting in the aforementioned idle mode of operation,
 as depicted in flow chart paths 197, 204 and 209 of the flow chart
 15 of FIGURE 5.

In the fine frequency error correction mode, signal FFR
 of FIGURE 7A controls the operation of charge pump stage 54 of
 FIGURE 10 for varying analog signal VCOCV. Variation of signal
 VCOCV causes the frequency of RCVCO 53 of FIGURE 1 to vary in a
 20 gradual manner and without switching steps of the switched
 capacitor, unlike in the coarse frequency error correction mode.

Signal NERR of FIGURE 6 is coupled through a word
 limiter 75 to a pulse generator 76. Limiter 75 produces an eight-
 bit, 2's complement word signal 75a from the least significant
 25 eight bits of signal NERR. Signal NERR is a 13-bit word signal.
 Should the magnitude of signal NERR be larger than what can be
 represented by eight-bit word signal 75a, signal 75a would be
 established at a value that is equal to the upper limit, positive or
 negative, of an eight-bit, 2's complement word. Word signal 75a
 30 is stored in a binary counter, not shown, of a pulse generator 76.
 Pulse generator 76 generates a pulse of a signal FFR_UP or a pulse
 of a signal FFR_DN, in accordance with bit SIGN of signal NERR.

A given pulse of output signal FFR_UP has a pulse
 width that is proportional to the magnitude of error signal NERR
 35 and is produced when the value of signal NERR is negative. Signal
 FFR_UP occurs when the frequency of signal Clk is lower than



required. Similarly, a given pulse of signal FFR_DN has a pulse
 5 width that is proportional to the magnitude of signal NERR and
 occurs when the frequency of signal Clk is higher than required.

Under the control of signal FFR, signal FFR_UP or
 FFR_DN of FIGURE 10 is selected and coupled through the
 corresponding one of a pair of two-input multiplexers 54a and
 10 54b and through the corresponding one of a pair of gates 54c and
 54d to the corresponding one of a pair of control terminals 54ca
 and 54cb of the corresponding one of a pair of switches SW3 and
 SW4. When the pulse of signal FFR_UP is generated, switch SW3
 couples a positive pulse current I3 to a terminal 54f. Similarly,
 15 when the pulse of signal FFR_DN is generated, switch SW4 couples
 a negative pulse current I4 to terminal 54f.

A capacitor Cint, formed using an integrating circuit
 fabrication technique, is coupled in parallel with a discrete
 capacitor Cext via switch SW1. This is done by having the selector
 20 of switch SW1 coupled to terminal 54f in the fine frequency
 correction mode. The control of switch SW1 is shown by the table
 in FIGURE 10. Consequently, capacitors Cext and Cint are charged
 in parallel, when signal FFR_UP is produced, by an amount that is
 proportional to the pulse width of signal FFR_UP. Capacitors Cext
 25 and Cint are discharged, in a similar manner, when signal FFR_DN
 occurs. Signal VCOCV is produced in capacitor Cext and is coupled
 to RCVCO 53 of FIGURE 2A.

Similarly to the coarse frequency error correction
 mode, and for similar reasons, during intervals MEASUREMENT,
 30 that occur during alternate periods H of signal HSRef of FIGURE 9b,
 the frequency of signal Clk does not change simultaneously with
 the measurement of the frequency error. Charging/discharging of
 capacitors Cint and Cext of FIGURE 10, in accordance with signal
 NERR, is enabled only during the other alternate periods intervals
 35 CONTROL of signal HSRef of FIGURE 9b. During operation in the
 fine frequency error correction mode, the difference between the



5 period length of signal ClkDiv and that of signal HSRef is brought to within 2 period length of signal Clk or approximately 0.2% of period H of signal HSRef.

The correction range that is produced by signal VCOCV in the fine frequency error correction mode is approximately $\pm 8\%$ of the entire frequency range of RCVCO 53 of FIGURES 2A-2C.

10 Therefore, advantageously, signal VCOCV has a sufficiently large range that overlaps each range of frequencies associated with a given switching step of signals $CF(4j+i)$ that occurs in the coarse frequency error correction mode. This is so because, as explained before, the range of frequencies associated with a given switching

15 step in the coarse frequency error correction mode is equal to approximately 4% of the entire frequency range of RCVCO 53. Advantageously, the correction range of signal VCOCV is still sufficiently small so that sensitivity to noise is reduced.

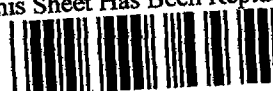
As explained before, when signal CONSISTENCY of

20 FIGURE 7B is not generated, the idle mode of operation occurs. The idle mode occurs when, for example, signal HSRef of FIGURE 1 is contaminated with noise. In the idle mode, switch SW1 of FIGURE 10 decouples capacitor Cext from terminal 54f. Therefore, capacitor Cext of FIGURE 10 is neither charged nor discharged and

25 signal VCOCV is maintained relatively constant. In the idle mode, signal VCOCV is coupled via a unity gain amplifier and a switch SW2 to capacitor Cint such that the capacitor voltage in terminal 54f of capacitor Cint tracks the voltage of signal VCOCV. The control of switch SW2 is shown by the table in FIGURE 10.

30 Assume that after an interruption interval in signal HSRef of FIGURE 1, normal operation signal HSRef is restored such that signal CONSISTENCY of FIGURE 7B is again produced. Because of the operation in the idle mode, signal VCOCV of FIGURE 10 is not disturbed and is more likely to be already maintained at the

35 approximately required level for steady state phase lock operation after the interruption interval in signal HSRef has



ended. Thus, transient condition in PLL 100 of FIGURE 1 may be,
5 advantageously, of short duration.

FIGURE 11 illustrates in more detail a phase detector
51 of FIGURE 1 that is used in a phase error correction mode of
operation. FIGURES 12a-12g illustrate corresponding waveforms.
Similar symbols and numerals in FIGURES 1, 2A-2C, 3-6, 7A, 7B, 8,
10 9a-9c, 10, 11 and 12a-12g indicate similar items or functions.
Detector 51 of FIGURE 11 includes a D-type flip-flop 51c that is
clocked by signal HSRef and reset by signal ClkDiv. Flip-flop 51c
generates a given pulse of signal FPH_UP of FIGURE 12c when the
leading edge of signal ClkDiv of FIGURE 12b lags behind that of
15 signal HSRef of FIGURE 12a. A D-type flip-flop 51d of FIGURE 11
is clocked by signal ClkDiv and reset by signal HSRef via a one-
shot multivibrator 51f. Flip-flop 51d generates a given pulse of
signal FPH_DN of FIGURE 12g, when the leading edge of signal
ClkDiv of FIGURE 12e leads that of signal HSRef of FIGURE 12a.
20 The pulse width of each of pulse signals FPH_UP and FPH_DN is
proportional to the phase difference. Only one of pulse signals
FPH_UP and FPH_DN can be generated at a given period H.

Pulse signal FPH_UP or FPH_DN of FIGURE 7B is
coupled via an "OR" gate 80 to a 3-bit binary counter 81. When
25 the pulse width of either pulse is smaller than 2 clock periods of
signal Clk, that is indicative of a relatively small phase error, an
output signal 81a is at a FALSE level. Signal 81a is coupled via an
inverter 82 to an input B of an "AND" gate 83. Frequency error
indicative signal 60a is coupled to a second input A of gate 83.
30 Signal 60a is generated when signal $|Nerr|$ is smaller than 2,
representing 2 clock periods of signal Clk.

For example, following operation in the fine frequency
error correction mode, when both the phase error is small, as
indicated by signal 81a being at the FALSE level, and the
35 frequency error is small, as indicated by the generation of signal
60a, gate 83 generates a signal FPH. As a result, a fine phase



error correction mode occurs. Flow chart paths 202, 206, 207 and
5 208 in the flow chart of FIGURE 5 depict the way the fine phase
error correction mode is obtained.

In the fine phase error correction mode, unlike in the
fine and coarse frequency error correction modes, the phase error
is both measured and corrected in each period H of signal HSRef of
10 FIGURE 9b. In the fine phase error correction mode, analog signal
VCOCV of FIGURE 10 that is proportional to the phase error is used
to acquire and maintain phase lock condition.

FIGURES 13a-13d illustrate waveforms useful for
explaining the operation in the fine phase error correction mode.
15 Similar symbols and numerals in FIGURES 1, 2A-2C, 3-6, 7A, 7B, 8,
9a-9c, 10, 11, 12a-12g and 13a-13d indicate similar items or
functions.

When signal FPH of FIGURE 7B is generated, signal
FPH_UP, alternatively, FPH_DN, of FIGURE 10 is coupled through
20 multiplexers 54a and 54b and through gates 54c and 54d to
terminals 54ca and 54cb of switches SW3 and SW4, respectively.
Signal FPH_UP, alternatively, FPH_DN is applied to capacitors Cint
and Cext in the following three operation sequence that occurs
during each period of signal ClkDiv of FIGURE 13B.

25 In the first operation of the aforementioned three
operation sequence, switch SW1 of FIGURE 10 is at a position
HOLD. Should the pulse of signal FPH_UP be generated, switch
SW3 would couple positive pulse current I3 to terminal 54f.
Similarly, should the pulse of signal FPH_DN be generated, switch
30 SW4 would couple negative pulse current I4 to terminal 54f.
Capacitor Cint is charged when signal FPH_UP is produced by an
amount that is proportional to its pulse width and is discharged
when signal FPH_DN is produced. Thus, capacitor Cint and
currents I3 and I4 operate as an integrator or a low pass loop
35 filter that develops in capacitor Cint a voltage proportional to the
phase error.



5 In the second operation of the sequence, a pulse
generator 85 of FIGURE 6 generates a pulse signal CHK of FIGURES
6 and 13c following the trailing edge of signal ClkDiv of FIGURE
13B. Pulse signal CHK of FIGURE 6 causes, in a manner not shown,
switch SW2 of FIGURE 10 to open and switch SW1 to couple
10 capacitor Cext to terminal 54f. Thus, capacitors Cint and Cext are
coupled in parallel. Therefore, the charge in capacitor Cext varies
in accordance with that of capacitor Cint and is determined by the
measured phase error. In this way, charge transfer occurs
between capacitors Cext and Cint.

15 In the third operation of the sequence, generator 85 of
FIGURE 6 generates a pulse signal INIT of FIGURES 6 and 13d
following pulse signal CHK of FIGURE 13c. Pulse INIT causes, in a
manner not shown, switch SW1 of FIGURE 10 to be in position
HOLD and switch SW2 to be closed. In this way, the initial
condition voltage is maintained in capacitor Cint the same as in
20 larger capacitor Cext in preparation for the next first operation in
the next three operation sequence the next three operation
sequence occurs in the next period of signal ClkDiv.
Advantageously, signal ClkDiv may suffer from less than, for
example, 2 ns jitter in the fine phase correction mode.

25 In accordance with another inventive feature, fine
frequency/phase control signal VCOCV of FIGURE 1 is also coupled
to a comparator 91. A signal OUT-OF-RANGE would be generated
by comparator 91 should the magnitude of signal VCOCV be
outside a predetermined voltage range. Signal OUT-OF-RANGE is
30 indicative of a situation in which signal VCOCV approaches a
magnitude that is outside a linear control range of operation of
RCVCO 53. When signal OUT-OF-RANGE is produced, PLL 100
begins operating in the coarse frequency control mode that was
explained before. Flow chart paths 214 and 215 in the flow chart
35 of FIGURE 5 depict such situation.



Should the phase error be large, resulting in a time
 5 difference between the leading edge of signal HSRef of FIGURE 12a
 and that of signal ClkDiv of FIGURE 12b or 12c that is equal to or
 greater than 2 clock periods of signal Clk of FIGURE 7B, signal 81a
 would be generated. Signal 81a causes a flip-flop 84 to be "set"
 and to generate an output signal PE_LAT. Signal PE_LAT is
 10 coupled to flip-flop 51c and 51d of phase detector 51 of FIGURE
 11 via "OR" gates 51a and 51b for terminating or producing a
 trailing edge of the then occurring pulse of signal FPH_UP or
 FPH_DN. Thus, advantageously, in the fine phase error correction
 mode, when detector 51 controls stage 54 of FIGURE 10, detector
 15 51 of FIGURE 11 is prevented from varying the frequency/phase
 of signal Clk by an excessive amount in each period of signal
 ClkDiv.

Signal 81a of FIGURE 7B at the TRUE level that is
 indicative of a large phase error is coupled to an input C of an
 20 "AND" gate 90. Signal CONSISTENCY that is indicative of consistent
 frequency error from one period H of signal HSRef of FIGURE 9b to
 the immediately next one, as explained before, is coupled to a
 second input A of gate 90 of FIGURE 7B. Signal 60a that is
 indicative of a small frequency error, when the value of signal
 25 $|Nerr|$ is smaller than 2, is coupled to a third input B of gate 90.
 Gate 90 generates a signal CPH_RST when all the three signals,
 81a, 60a and CONSISTENCY, are generated. Signal CPH_RST is
 coupled to a clock input of a D-type flip-flop 91. An output Q of
 flip-flop 91 is coupled to an input D of a D-type flip-flop 92 that
 30 produces a pulse signal RST when the leading edge of signal HSRef
 occurs following the generation of signal CPH_RST.

Signal RST is coupled to +N counter 52 of FIGURE 1 for
 presetting the flip-flops, not shown, of counter 52 in a manner to
 provide an immediate phase lock between signals HSRef and
 35 ClkDiv. Thus, signal RST provides a coarse phase error correction
 mode of operation. Flow chart paths 210, 211 and 212 in the flow

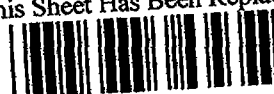


chart of FIGURE 5 depict the way the coarse phase correction mode is obtained. This mode can occur when, for example, the phase of signal HSRef of FIGURE 1 that is produced in a video tape recorder, changes abruptly, during a vertical retrace interval of a playback mode. The coarse phase error correction is accomplished via a signal path between RCVCO 53 of FIGURE 1 and phase detector 51 in a manner that bypasses the signal path of signal VCOCV. As a result of the abrupt or coarse phase correction, the phase of signal ClkDiv is aligned with that of signal HSRef without significantly affecting the phase of signal Clk. In this way, advantageously, transient disturbance in RCVCO 53 is eliminated or significantly reduced.

Should signal 81a of FIGURE 7B that is indicative of a large phase error be generated and signal CONSISTENCY, that is indicative of a stable sync signal HSRef, not be generated, signal RST would not be generated and the idle mode of operation would occur. Flow chart path 213 in the flow chart of FIGURE 5 depicts this way in which the idle mode is obtained. The advantage of operating in the idle mode and preventing the coarse phase error correction when signal CONSISTENCY of FIGURE 7B is not generated is that disturbance or transient in PLL 100 of FIGURE 1 may be reduced. Such disturbance may be reduced when, for example, the duration of the interruption in signal HSRef is short.

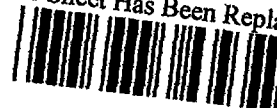
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**WHAT IS CLAIMED IS:**

- 5 1. An apparatus for generating an oscillatory signal
that is locked to an input signal, comprising:
 an amplifier;
 a plurality of switched reactive elements selectively
coupled in a positive feedback path formed between an output
10 and an input of said amplifier for generating said oscillatory signal
having a frequency that is selected from a corresponding portion
of a range of frequencies in accordance with a selection of said
switched reactive elements;
- first means responsive to said oscillatory signal for
15 measuring a frequency error between said oscillatory and input
signals and for generating a first switching control signal that is
coupled to a switching arrangement associated with said switched
reactive elements to select said switched reactive elements in
accordance with said frequency error such that when said
20 frequency error exceeds a first value, the selection of said
switched reactive element varies in switching steps of a coarse
frequency correction mode of operation, to reduce said frequency
error progressively in successive switching steps; and
- second means responsive to said oscillatory signal and
25 to said synchronizing signal for generating a second control signal
that is coupled to a control input of said amplifier for varying said
frequency of said oscillatory signal within said corresponding
portion of said range to correct said frequency error in a fine
error correction mode of operation when said frequency error
30 does not exceed said first value, without varying the selection of
said switched reactive elements.

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2. An apparatus according to Claim 1 further
5 comprising, a comparator responsive to said second control signal
and to a signal at a reference level and coupled to said first means
for initiating operation in said coarse frequency error correction
mode of operation, when said second control signal is outside a
predetermined correction range of said oscillator.
10
3. An apparatus according to Claim 1 wherein said
second control signal generating means comprises a frequency
detector for generating a third signal that is indicative of said
frequency error and a phase detector for generating a fourth
15 signal that is indicative of said phase error said third and fourth
signals being selectively coupled to said control input of said
amplifier to form said second control signal at said control input,
such that when said frequency error is smaller than said first
value and larger than a second value, said third signal is applied
20 to said oscillator in a fine frequency error correction mode of
operation and when said frequency error is smaller than said
second value said fourth signal is applied to said oscillator in a
fine phase error correction mode of operation.
- 25 4. An apparatus according to Claim 1 wherein said
second control signal is an analog signal.
5. An apparatus according to Claim 1 wherein a given
switched reactive element comprises a switched capacitor.
30
6. An apparatus according to Claim 1 wherein said
first means comprises, means for generating a coded signal and a
decoder for decoding said coded signal to generate a plurality of
switch control signals that are applied to said switches in a
35 manner to vary said frequency of said oscillator signal
monotonically in each switching step.

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7. An apparatus according to Claim 1 wherein an
5 impedance of a given switched reactive element determines said
frequency of said oscillatory signal.

8. Apparatus for generating an oscillatory signal that
is locked to an input signal, comprising:

10 a controllable oscillator for generating said oscillatory
signal;

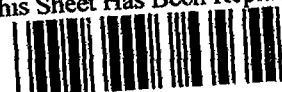
a plurality of switched reactive elements selectively
coupled to a feedback path of said oscillator for controlling said
oscillatory signal in accordance with the selection of said switched
15 reactive elements;

means coupled to said switched reactive elements for
sequentially selecting from said switched reactive elements a
given switched reactive element that is to be coupled to said
feedback path and a given switched reactive element that is to be
20 decoupled from said feedback path in a manner to reduce an error
between said oscillatory and synchronizing signals in a given
sequential step of a coarse error correction mode of operation;

means responsive to said oscillatory signal and to said
synchronizing signal for generating a first signal that is indicative
25 of said error therebetween, said first signal being coupled via a
loop filter to a control input of said oscillator to control said
oscillator in a fine error correction mode of operation when said
error is smaller than a first value such that in said fine error
correction mode of operation the selection of said switched
30 reactive elements does not vary; and

a comparator responsive to said filtered first signal
and to a signal at a reference level and coupled to said switched
reactive element selecting means for initiating operation in said
coarse error correction mode of operation, when said filtered first
35 signal is outside a predetermined correction range of said
oscillator.

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9. An apparatus for generating an oscillatory signal
5 that is locked to an input signal, comprising:
a controllable oscillator for generating said oscillatory
signal;

a source of said input signal at a frequency that is
related to a scanning frequency;
10 a plurality of selectable switched reactive elements
coupled in a feedback path of said oscillator;
a frequency detector responsive to said oscillatory and
synchronizing signals for generating a first signal that is indicative
of a frequency error therebetween;

15 a charge pump responsive to said first signal for
generating a filtered second signal that is coupled to a control
input of said oscillator for varying said frequency of said
oscillatory signal in a fine frequency error correction mode of
operation to correct for said frequency error in a feedback loop
20 manner without varying a selection of said switched reactive
elements;

means for initiating operation in a coarse frequency
error correction mode in accordance with said first signal via a
signal path that bypasses said charge pump when said frequency
25 error exceeds a first predetermined magnitude such that in said
coarse frequency error correction mode the selection of said
switched reactive elements varies in a manner to reduce said
frequency error; and

a comparator responsive to said second signal of said
30 charge pump and to a signal at a reference level and coupled to
said switched reactive elements for initiating operation in said
coarse frequency error correction mode of operation when a
difference between said second signal and said signal at said
reference level is outside a normal operation range of values.

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10. An oscillator that is locked to a synchronizing
5 signal, comprising:
a first amplifier;
a first switched reactive element selectively coupled in
a first positive feedback path formed between an output and an
input of said first amplifier;
10 a second amplifier;
a second switched reactive elements selectively
coupled in a second positive feedback path formed between an
output and an input of said second amplifier for producing a pair
of differentially symmetrical signals in said first and second
15 positive feedback paths, respectively;
means for combining said pair of differentially
symmetrical signals to generate an oscillatory signal;
a source of said synchronizing signal; and
means coupled to said switched reactive elements for
20 varying the selection of said switched reactive elements in a given
switching step in a manner to reduce a frequency error of said
oscillatory signal with respect to that of said synchronizing signal
in a frequency correction mode of operation, such that, when the
selection of said first switched reactive element varies in said first
25 positive feedback path the selection of said second switched
reactive element also varies in said second positive feedback path
in a manner to maintain said pair of signals differentially
symmetrical.
- 30 11. An oscillator according to Claim 10 further
comprising, means responsive to said oscillatory and
synchronizing signals for generating a gain control signal that is
coupled to a gain control input of one of said amplifier for
reducing one of a frequency error and a phase error in a fine
35 error correction mode of operation.

This Sheet Has Been Replaced





- 5 12. An apparatus according to Claim 11 wherein, in said given switching step, said gain control signal has a variation range that produces a larger frequency variation range in said oscillatory signal than that produced by varying the selection of said switched reactive elements in said given switching step.
- 10 13. An apparatus according to Claim 11 wherein said gain control signal generating means comprises a phase detector for providing a phase correction in a fine phase correction mode of operation.
- 15 14. An apparatus according to Claim 11 wherein said gain control signal generating means comprises a frequency detector for providing a frequency correction in a fine frequency correction mode of operation.
- 20 15. An apparatus according to Claim 10 wherein said given switching step occurs sequentially at a rate that is equal to a multiple of a horizontal deflection frequency.
- 25 16. An apparatus according to Claim 10 wherein at least one of said switched reactive elements comprises a switched capacitors that are formed by an integrated circuit fabrication technique.
- 30 17. An apparatus according to Claim 10 wherein said combining means comprises a differential amplifier having an inverting input terminal that is responsive to one of said pair of signals and a noninverting input terminal that is responsive to the other one of said pair of signals.

