

Description

The invention relates to a protection circuit for protecting a transistor from overloading, comprising

— first means for generating a first signal which is a measure of the collector current of the transistor,

— second means for generating a second signal which is a measure of the collector-emitter voltage of the transistor, this second signal having a constant value above a given collector-emitter voltage, which is referred to as knee voltage, and

— third means limiting the collector current of the transistor if a combination of the first and second signals exceeds a certain threshold value.

Such a protection circuit can, for example, be used in integrated power amplifiers for audio equipment. The output transistors of such power amplifiers must be operated within the Safe Operating Area Rating (SOAR) to prevent the transistors from being damaged by overloading.

Such a protection circuit is, for example, used in the integrated audio amplifier TDA 1520, described in Philips Data-Handbook: Integrated Circuits, January 1983. Therein, the first means comprises a first resistor included in the collector or the emitter lead of the transistor. A first signal is derived from the voltage across this resistor, which signal consequently is proportional to the current through the transistor. The second means comprise a voltage divider formed by second and third resistors and arranged between the collector and the emitter of the transistor. A second signal is derived from the voltage across the second resistor, which second signal is consequently proportional to the collector-emitter voltage of the transistor. Above a given collector-emitter voltage, which is referred to as knee voltage, the voltage across the second resistor is limited by a Zener diode arranged in parallel therewith, so that the second signal has a constant value above the knee voltage.

The first and second signals are added together whereafter this sum signal is compared with a threshold value. If the sum signal becomes greater than the threshold value, then a transistor is rendered conductive which diverts base current from the output transistor and consequently limits the current through the output transistor.

From the fact that when the protection becomes operative the sum of the first and second signals is controlled in such manner that this sum is equal to the threshold value, it follows that the limited value of the current through the output transistor is equal to the difference between a fixed current which is proportional to the threshold value and a variable current which is proportional to the collector-emitter voltage of the transistor.

With very small collector-emitter voltages the second signal is so small as to be disregarded. In that case the protection becomes operative if the first signal, which is proportional to the collector current, becomes greater than the threshold value. The implication is that the maximum cur-

rent through the output transistor is proportional to the threshold value.

Since the voltage across the second resistor is limited by the zener diode, a small residual current may continue to flow through the output transistor in the event of collector-emitter voltages above the knee voltage. This residual current is necessary to ensure that the circuit can operate correctly upon application of the supply voltage, as the load, for example a loudspeaker, is coupled to the output of the output transistor via a capacitor. Upon switch-on a certain current is required to charge this capacitor. The residual current is also required to prevent distortion of the output signal in the event of a large voltage swing. This residual current is equal to the difference between the maximum current through the transistor, which is proportional to the threshold value, and a fixed current which is proportional to the knee voltage.

Now the residual current is much smaller, for example by a factor of 20, than the maximum current through the output transistor. Consequently, the residual current is formed by the difference between two currents which are each much larger than the residual current itself, in the present example 20 and 19 times larger, respectively. As a result thereof, the residual current is highly dependent on variations in these currents. A variation of, for example, 5% in one of the currents causes a variation of 100% in the residual current. Precisely in the area above the knee voltage with high collector-emitter voltages an excessive residual current may easily result in the output transistor being damaged. A too small residual current has for its result that the output signal is distorted in the event of a large voltage swing or that the circuit cannot build-up to proper operation upon application of the supply voltage.

It is therefore an object of the invention to provide a protection circuit with which an improved protection at high collector-emitter voltages is obtained. A circuit of the type set forth in the opening paragraph is therefore characterized in that

— the second signal is a measure of the difference between the knee voltage and the collector-emitter voltage, and

— the combination of the first and second signals is formed by the difference between the first and second signals.

The invention is based on the recognition that when the protection becomes operative the current through the output transistor need not be controlled in such manner that it becomes equal to the difference between a fixed current and a variable current which depends on the collector-emitter voltage, but can be made equal to the sum of a fixed current and a variable current which depends on the collector-emitter voltage, it being a requirement that this variable current becomes equal to zero above the knee voltage. Then the residual current through the output transistor is equal to a fixed current, which is variation-dependent to a much lesser extent. This is realised by

using the measures according to the invention. The second signal is equal to zero above the knee voltage. When the protection becomes operative at collector-emitter voltages above the knee voltage, the first signal is controlled in such manner that it becomes equal to the threshold value, so that the residual current is proportional to the threshold value.

Such a protection circuit may be further characterized in that the first means comprise a first resistor included in the collector or the emitter lead of the transistor and a first voltage-current converter converting the voltage across the first resistor into a current proportional thereto, that the second means comprise a second voltage-current converter converting the difference between the collector-emitter voltage and the knee voltage into a current proportional thereto and that the third means comprise a control amplifier which so limits the current through the transistor that the difference between the output currents of the first and second voltage-current converters is equal to a threshold current carried by a current source.

The invention will now be described in greater detail, by way of example, with reference to the accompanying drawings in which

Fig. 1 shows the basic circuit diagram of an example of a protection circuit according to the invention,

Fig. 2 shows the collector current-collector-emitter voltage characteristic of the protection circuit of Fig. 1,

Fig. 3 shows the detailed construction of a particular protection circuit according to the invention,

Fig. 4 shows the collector current-collector-emitter voltage characteristic associated with the circuit shown in Fig. 3, and

Fig. 5 shows an amplifier circuit comprising protection circuits according to the invention.

Fig. 1 shows the basic circuit diagram of an example of a protection circuit according to the invention. The output transistor T_1 to be protected is connected by means of its collector to the output 2 of the circuit to which a load impedance 4 is coupled via a capacitor 3. The emitter of transistor T_1 is connected to the negative supply terminal 5, in this case ground, via a resistor R_1 . The resistor R_1 has a very small resistance value of, for example, 0.03 Ohm, which can be constituted by the wire connection between the emitter of transistor T_1 and the supply terminal 5. The transistor T_1 must be operated within the so-called SOAR to prevent the transistor T_1 from being damaged by overloading due to an excessively high current, either in combination or not in combination with an excessively high voltage. In order to ensure operation within the SOAR-range the circuit must be protected. To that end the emitter current I_E of transistor T_1 is converted by

resistor R_1 into a voltage which is applied to the non-inverting input 7 of a voltage-current converter 6, whose inverting input 8 is connected to ground. The output current I_1 of the voltage-current converter 6 is therefore $I_1 = aI_E$, a being a constant which is determined by the transconductance of the V/I-converter 6 and the resistance value of resistor R_1 .

The collector-emitter voltage V_{CE} of transistor T_1 is applied to the inverting input 10 of a voltage-current converter 9. The non-inverting input 11 of this V/I-converter 9 carries a constant voltage V_{KN} , the so-called knee voltage. The output current I_2 of the V/I-converter 9 is therefore equal to $I_2 = b(V_{KN} - V_{CE})$, b being a constant determined by the transconductance of the V/I-converter 9. A diode 12 which is cut-off at the instant at which the output current reverses, that is to say at the instant at which the collector-emitter voltage V_{CE} becomes larger than the knee voltage V_{KN} , is included in the output lead of the V/I-converter 9. Consequently, the V/I-converter 9 does not produce an output current for collector-emitter voltages V_{CE} larger than the knee voltage V_{KN} .

The output leads of the V/I-converters 6 and 9 are connected to a common point 13, which is coupled to a current source 14 carrying a current I_D and are further connected via a diode 15 to the inverting input 17 of a control amplifier 16, whose non-inverting input 18 carries a drive signal for the output transistor T_1 . The output of the amplifier 16 is coupled to the base of the output transistor T_1 . The direction of the output current I_2 of the V/I-converter 9 is opposite to that of I_1 from the V/I-converter 6, so that the difference $I_M = I_1 - I_2$ between these output currents is available at the point 13. This current I_M is now compared with the current I_D carried by the current source 14. If the current I_M is smaller than the current I_D then the protection is not operative. The difference between the currents I_M and I_D is then supplied by current supply means, not shown for the sake of simplicity, which are switched off as soon as the protection circuit becomes operative. The protection circuit becomes operative when the current I_M becomes larger than the current I_D . The difference between these currents then flows through the inverting input 17 of the control amplifier 16. This control amplifier 16 now controls the output transistor T_1 in such manner that the current I_M becomes equal to the current I_D . In that case it holds that:

$$I_D = aI_E - b(V_{KN} - V_{CE}) \text{ for } V_{CE} < V_{KN} \quad (1a)$$

$$I_D = aI_E \text{ for } V_{CE} \geq V_{KN} \quad (1b)$$

From this it follows for the current I_E as a function of the collector-emitter voltage V_{CE} that:

$$I_E = \frac{I_D}{a} + \frac{b}{a} (V_{KN} - V_{CE}) \text{ for } V_{DE} < V_{KN} \quad (2a)$$

$$I_E = \frac{I_D}{a} \text{ for } V_{CE} \geq V_{KN} \quad (2b)$$

Fig. 2 shows the I_D/V_{CE} characteristic determined by formulae 2a and 2b. For a very small V_{CE} the current is limited to the maximum current

$$I_E \text{ max} = \frac{I_D}{a} + \frac{b}{a} V_{KN}.$$

The limit value of the current I_E decreases linearly versus increasing V_{CE} . Above the knee voltage V_{KN} a small residual current which is defined by formula 2b continues to flow through transistor T_1 . This residual current ensures that the circuit is capable of supplying the current required for the quiescent setting when the supply is switched on. For that purpose it is *inter alia* necessary that upon switch on of the supply voltage a small current flows to charge the capacitor 3 (see Fig. 1). A small residual current must also flow to prevent, in the event of a large voltage swing, distortion which would otherwise occur because of the fact that the transistor T_1 becomes currentless. The residual current is no longer formed, as in the prior art protection circuit, by the difference between two comparatively large currents but is directly determined by the threshold current I_D . The magnitude of the residual current depends therefore to a much lesser extent on variations, so that the probability that the output transistor T_1 is damaged by overloading at high collector-emitter voltages is significantly reduced.

A particular protection circuit will now be described in greater detail with reference to Fig. 3. Herein T_1 is again the transistor to be protected, whose collector is connected to the output 2 and whose emitter is connected to ground via a resistor R_1 . The resistor R_1 forms part of a current mirror circuit forming the first voltage-current converter. The current mirror circuit comprises a first path, incorporating a current source 20, a diode-connected transistor T_2 , a transistor T_3 and the resistor R_1 and a second path incorporating transistors T_4 and T_5 and resistor R_2 . The transistors T_2 and T_4 have commoned bases, whilst the base of transistor T_3 is connected to the collector of transistor T_5 and the base of transistor T_5 is connected to the collector of transistor T_3 . As the collector current of transistor T_4 is substantially equal to that of transistor T_5 , and as the collector current of transistor T_2 is substantially equal to that of transistor T_3 , the sum of the base-emitter voltages of transistors T_3 and T_4 is equal to the sum of those of transistors T_2 and T_5 . The collector current of transistor T_4 is therefore such that the voltages across the resistors R_1 and R_2 are substantially equal. In response to the emitter current I_E of transistor T_1 there will therefore flow

in the collector circuit of transistor T_4 , disregarding a setting direct current term due to current source 20, and disregarding the collector current of transistor T_5 , a current which is equal to

$$\frac{R_1}{R_2} \cdot I_E$$

The direct current term is compensated for by an equally large term in the current carried by current source 25, which however plays no part in the operation of the protection and is consequently omitted from the further calculations.

The collector of transistor T_1 is coupled via a resistor R_3 and a diode 21 to the input of a current mirror formed by the transistors T_7 , T_8 and T_9 . In addition, a current source 22 carrying a current kI_D is coupled to the input of the current mirror. The commoned emitters of the transistors T_7 , T_8 are connected to the emitter of a transistor T_{10} , the base of which carries a reference voltage V_Z . The output current of the current mirror T_7 , T_8 , T_9 is applied to the resistor R_2 .

The voltage at the cathode of diode 21 is substantially $V_Z - 3V_{BE}$, wherein the V_{BE} s are the base-emitter voltages of transistors T_8 , T_9 and T_{10} . The diode 21 is therefore non-conductive for voltages at the output 2 less than $V_Z - 2V_{BE}$. In such a case the current applied to resistor R_2 from mirror T_7 , T_8 , T_9 , is exactly equal to the current kI_D carried by current source 22. The total collector current I_M of transistor T_4 is then equal to

$$I_M = \frac{R_1}{R_2} \cdot I_E - kI_D.$$

This current is now first reproduced with the aid of a current mirror comprising transistors T_{11} and T_{12} and thereafter compared with the current I_D carried by a current source 25, which in this example is further coupled schematically for the sake of simplicity to a control amplifier 27 via a diode 26. If now the current I_M becomes greater than the current I_D then the protection circuit becomes operative and the control amplifier so controls the current I_E through the output transistor T_1 that the current I_M becomes equal to the current I_D . The current I_E is thereby limited to the maximum value

$$I_E \text{ max} = \frac{R_2}{R_1} (1 + k) I_D$$

For voltages at the output 2 higher than $V_Z - 2V_{BE}$ diode 21 starts to conduct, so that with increasing collector-emitter voltage a portion of the current kI_D will flow through the resistor R_3 . As a result thereof the limit value of the emitter current I_E will decrease linearly with increasing collector-emitter voltages V_{CE} .

If the voltage at the output 2 reaches the value of the knee voltage $V_K = V_Z - 2V_{BE} + kI_D R_3$, then

the current I_D carried by current source 22 flows completely through resistor R_3 and the current mirror T_7, T_8, T_9 becomes currentless. The current I_M then becomes equal to

$$I_M = \frac{R_1}{R_2} I_E,$$

so that the current I_E is limited to a residual value equal to

$$I_E = \frac{R_2}{R_1} \cdot I_D.$$

For the sake of completeness Fig. 4 illustrates the associated $I_E - V_{CE}$ characteristic together with the characteristic values.

Fig. 5 shows an amplifier circuit provided with protection circuits according to the invention. The amplifier comprises a first stage 30 which evidences the character of a voltage-current converter and comprises a pair of transistors T_{15} and T_{16} which are connected as a differential amplifier and whose base electrodes constitute the inverting and the non-inverting inputs. The emitters of the transistors T_{15} and T_{16} are connected to the positive supply terminal 32 via a current source 31. The collectors of the transistors T_{15}, T_{16} are connected to the output 36 of this stage 30 via a current mirror comprising T_{17}, T_{18}, T_{19} , resistors 33 and 34 and current source 35. The output 36 forms at the same time the input 36 of a Miller stage 40, which has the character of a current-voltage converter. The input 36 is further connected to output 2 via a compensation-capacitance 46. This stage 40 comprises a control transistor T_{20} with emitter resistor 42, which is driven by means of the emitter follower configuration formed by transistor T_{21} and current source 41 and whose collector is connected to the positive supply terminal 32 via the diodes 42, 43 and 44 and a current source 45. The output stage is constructed as a quasi-complementary output stage with NPN output transistors T_1 and T_{25} , which form Darlington transistors with NPN transistors T_{26} and T_{27} respectively. The quasi-complementary behaviour is obtained by adding the PNP transistors T_{28} and T_{29} as shown in the Figure. Output transistor T_1 is protected by a circuit 50 which is almost wholly identical to the protection circuit of Fig. 3 and in which corresponding components are given the same reference numerals.

Before it is compared with the current I_D carried by current source 25, the current I_M is reproduced with the aid of a current mirror comprising transistors T_{30}, T_{31} and resistors 51 and 52. The difference between the currents I_M and I_D is applied to the series arrangement of a resistor 53 and capacitor 54. The voltage across this series arrangement is applied to resistor 55 via the amplifier T_{32} which is connected as an emitter follower. With a view to driving transistor T_1 , the

emitter current of transistor T_{32} must still be inverted before presentation to the input 36 of the control stage. This is accomplished by connecting the resistor 55 to the input of the current mirror T_{17}, T_{18}, T_{19} , which causes that current mirror to invert the emitter current of transistor T_{32} before presenting it to input 36.

In the protection circuit 50 the base of transistor T_{32} is clamped with the aid of a transistor T_{33} relative to a point which carries reference voltage V_R . This measure has for its object to prevent the protection circuit 50 from becoming active when there is no need for the protection to operate. The current I_M is then smaller than the current I_D carried by current source 25. The transistor T_{33} is then kept in the conducting stage by the superfluous current from current source 25. The voltage V_R is therefore such that transistor T_{32} does not conduct when the protection is not active. Transistor T_{33} is rendered non-conductive at the instant at which the protection becomes operative and transistor T_{32} starts to conduct.

Output transistor T_{25} is protected in a similar way by means of a circuit 50A, which corresponds to a large extent to circuit 50 and in which corresponding components are given the same reference numerals with the addition of the index A. The mode of operation of circuit 50A is the same as that of circuit 50, with the exception that the transistors of the current mirrors T_{2A} to T_{5A} and T_{7A} to T_{10A} are of the opposite conductivity types. As a result thereof the current I_M must not first be inverted by a current mirror before it is applied to the base of transistor T_{32A} . In view of the complementary drive of transistor T_{25} the resistor 55A is directly connected to the input 36 of the control amplifier T_{20}, T_{21} .

Claims

1. A protection circuit for protecting a transistor (T_1) from overloading, comprising

— first means ($R_1, 6$) for generating a first signal (I_1) which is a measure of the collector current of the transistor (T_1),

— second means (9) for generating a second signal (I_2) which is a measure of the collector-emitter voltage of the transistor (T_1), this second signal (I_2) having a constant value above a given collector-emitter voltage, which is referred to as knee voltage (V_{KN}), and

— third means (14, 15, 16) limiting the collector current of the transistor (T_1) if a combination of the first (I_1) and second (I_2) signals exceeds a certain threshold value (I_D), characterized in that

— the second signal (I_2) is a measure of the difference between the knee voltage (V_{KN}) and the collector-emitter voltage and

— the combination of the first (I_1) and second (I_2) signals is formed by the difference (I_M) between the first (I_1) and second (I_2) signals. (Fig. 1).

2. A protection circuit as claimed in Claim 1, characterized in that the first means comprise a

the current I_D carried by current source 22 flows completely through resistor R_3 and the current mirror T_7 , T_8 , T_9 becomes currentless. The current I_M then becomes equal to

$$I_M = \frac{R_1}{R_2} I_E$$

so that the current I_E is limited to a residual value equal to

$$I_E = \frac{R_2}{R_1} \cdot I_D$$

For the sake of completeness Fig. 4 illustrates the associated $I_E - V_{CE}$ characteristic together with the characteristic values.

Fig. 5 shows an amplifier circuit provided with protection circuits according to the invention. The amplifier comprises a first stage 30 which evidences the character of a voltage-current converter and comprises a pair of transistors T_{15} and T_{16} which are connected as a differential amplifier and whose base electrodes constitute the inverting and the non-inverting inputs. The emitters of the transistors T_{15} and T_{16} are connected to the positive supply terminal 32 via a current source 31. The collectors of the transistors T_{15} , T_{16} are connected to the output 36 of this stage 30 via a current mirror comprising T_{17} , T_{18} , T_{19} , resistors 33 and 34 and current source 35. The output 36 forms at the same time the input 36 of a Miller stage 40, which has the character of a current-voltage converter. The input 36 is further connected to output 2 via a compensation-capacitance 46. This stage 40 comprises a control transistor T_{20} with emitter resistor 42, which is driven by means of the emitter follower configuration formed by transistor T_{21} and current source 41 and whose collector is connected to the positive supply terminal 32 via the diodes 42, 43 and 44 and a current source 45. The output stage is constructed as a quasi-complementary output stage with NPN output transistors T_1 and T_{25} , which form Darlington transistors with NPN transistors T_{26} and T_{27} respectively. The quasi-complementary behaviour is obtained by adding the PNP transistors T_{28} and T_{29} as shown in the Figure. Output transistor T_1 is protected by a circuit 50 which is almost wholly identical to the protection circuit of Fig. 3 and in which corresponding components are given the same reference numerals.

Before it is compared with the current I_D carried by current source 25, the current I_M is reproduced with the aid of a current mirror comprising transistors T_{30} , T_{31} and resistors 51 and 52. The difference between the currents I_M and I_D is applied to the series arrangement of a resistor 53 and capacitor 54. The voltage across this series arrangement is applied to resistor 55 via the amplifier T_{32} which is connected as an emitter follower. With a view to driving transistor T_1 , the

emitter current of transistor T_{32} must still be inverted before presentation to the input 36 of the control stage. This is accomplished by connecting the resistor 55 to the input of the current mirror T_{17} , T_{18} , T_{19} , which causes that current mirror to invert the emitter current of transistor T_{32} before presenting it to input 36.

In the protection circuit 50 the base of transistor T_{32} is clamped with the aid of a transistor T_{33} relative to a point which carries reference voltage V_R . This measure has for its object to prevent the protection circuit 50 from becoming active when there is no need for the protection to operate. The current I_M is then smaller than the current I_D carried by current source 25. The transistor T_{33} is then kept in the conducting stage by the superfluous current from current source 25. The voltage V_R is therefore such that transistor T_{32} does not conduct when the protection is not active. Transistor T_{33} is rendered non-conductive at the instant at which the protection becomes operative and transistor T_{32} starts to conduct.

Output transistor T_{25} is protected in a similar way by means of a circuit 50A, which corresponds to a large extent to circuit 50 and in which corresponding components are given the same reference numerals with the addition of the index A. The mode of operation of circuit 50A is the same as that of circuit 50, with the exception that the transistors of the current mirrors T_{2A} to T_{5A} and T_{7A} to T_{10A} are of the opposite conductivity types. As a result thereof the current I_M must not first be inverted by a current mirror before it is applied to the base of transistor T_{32A} . In view of the complementary drive of transistor T_{25} the resistor 55A is directly connected to the input 36 of the control amplifier T_{20} , T_{21} .

Claims

1. A protection circuit for protecting a transistor (T_1) from overloading, comprising

— first means (R_1 , 6) for generating a first signal (I_1) which is a measure of the collector current of the transistor (T_1),

— second means (9) for generating a second signal (I_2) which is a measure of the collector-emitter voltage of the transistor (T_1), this second signal (I_2) having a constant value above a given collector-emitter voltage, which is referred to as knee voltage (V_{KN}), and

— third means (14, 15, 16) limiting the collector current of the transistor (T_1) if a combination of the first (I_1) and second (I_2) signals exceeds a certain threshold value (I_D),

characterized in that

— the second signal (I_2) is a measure of the difference between the knee voltage (V_{KN}) and the collector-emitter voltage and

— the combination of the first (I_1) and second (I_2) signals is formed by the difference (I_M) between the first (I_1) and second (I_2) signals. (Fig. 1).

2. A protection circuit as claimed in Claim 1, characterized in that the first means comprise a



first resistor (R_1) included in the collector or the emitter lead of the transistor (T_1) and a first voltage-current converter (6) converting the voltage across the first resistor (R_1) into a current (I_1) proportional thereto, that the second means comprise a second voltage-current converter (9) converting the difference between the collector-emitter voltage and the knee voltage (V_{KN}) into a current (I_2) proportional thereto and that the third means comprise a control amplifier (16) which so limits the current through the transistor (T_1) that the difference (I_M) between the output currents of the first (6) and second (9) voltage-current converters is equal to a threshold current (I_0) carried by a current source (14). (Fig. 1).

3. A protection circuit as claimed in Claim 2, characterized in that the first voltage-current converter is formed by a first current mirror circuit having an input circuit which comprises at least the series arrangement of a current source (20), a second transistor (T_2) and the first resistor (R_1) and an output circuit which comprises at least the series arrangement of a third transistor (T_4) and a second resistor (R_2), that the second voltage-current converter is formed by a second current mirror circuit having an input circuit which comprises at least the series arrangement of a current source (22) and a third transistor (T_7) and an output circuit which comprises at least a fourth transistor (T_8), the input and output circuits having a common fifth transistor (T_{10}) the control electrode of which carries a reference voltage (V_2), that the input circuit of the second current mirror circuit is further coupled via the series arrangement of a diode (21) and a third resistor (R_3) to the collector or the emitter of the transistor (T_1) to be protected and that the output circuit of the second current mirror circuit is further coupled to the second resistor (R_2) in the output circuit of the first current mirror circuit. (Fig. 3).

Patentansprüche

1. Schutzschaltung zum Schützen eines Transistors (T_1) gegen Überlastung, mit

— ersten Mitteln (R_1 , 6) zum Erzeugen eines ersten Signals (I_1), das ein Maß für den Kollektorstrom des Transistors (T_1) ist,

— zweiten Mitteln (9) zum Erzeugen eines zweiten Signals (I_2), das ein Maß für die Kollektor-Emitter-Spannung des Transistors (T_1) ist, wobei dieses zweite Signal (I_2) einen konstanten Wert über einer bestimmten Kollektor-Emitter-Spannung, der sog. Knie-Spannung (V_{KN}), hat, und

— dritten Mitteln (14, 15, 16) zum Begrenzen des Kollektorstroms des Transistors (T_1), wenn eine Kombination der ersten (I_1) und zweiten (I_2) Signale einen bestimmten Schwellenwert (I_0) überschreitet, dadurch gekennzeichnet, daß

— das zweite Signal (I_2) ein Maß für den Unterschied zwischen der Knie-Spannung (V_{KN}) und der Kollektor-Emitter-Spannung ist, und

— die Kombination der ersten (I_1) und zweiten (I_2) Signale durch den Unterschied (I_M) zwischen den ersten (I_1) und zweiten (I_2) Signalen gebildet wird. (Fig. 1).

2. Schutzschaltung nach Anspruch 1, dadurch gekennzeichnet, daß die ersten Mittel einen ersten Widerstand (R_1) in der Kollektor- oder Emitterleitung des Transistors (T_1) und einen ersten Spannungs-Strom-Wandler (6) zum Umsetzen der Spannung am ersten Widerstand (R_1) in einen dazu proportionalen Strom (I_1) enthalten, daß die zweiten Mittel einen zweiten Spannungs-Strom-Wandler (9) zum Umsetzen des Unterschieds zwischen der Kollektor-Emitter-Spannung und der Knie-Spannung (V_{KN}) in einen dazu proportionalen Strom (I_2) und die dritten Mittel einen Regelverstärker (16) enthalten, der den Strom durch den Transistor (T_1) derart begrenzt, daß der Unterschied (I_M) zwischen den Ausgangsströmen der ersten (6) und zweiten (9) Spannungs-Strom-Wandler gleich einem Schwellenstrom (I_0) einer Stromquelle 14 ist. (Fig. 1).

3. Schutzschaltung nach Anspruch 2, dadurch gekennzeichnet, daß der erste Spannungs-Strom-Wandler durch eine erste Stromspiegelschaltung mit einer Eingangsschaltung, die wenigstens die Reihenschaltung aus einer Stromquelle (20), einem zweiten Transistor (T_2) und dem ersten Widerstand (R_1) enthält, und mit einer Ausgangsschaltung gebildet wird, die wenigstens die Reihenschaltung eines dritten Transistors (T_4) und einem zweiten Widerstand (R_2) enthält, daß der zweite Spannungs-Strom-Wandler durch eine zweite Stromspiegelschaltung mit einer Eingangsschaltung, die wenigstens die Reihenschaltung aus einer Stromquelle (22) und einem dritten Transistor (T_7) enthält, und mit einer Ausgangsschaltung gebildet wird, die wenigstens einen vierten Transistor (T_8) enthält, wobei die Eingangs- und Ausgangsschaltungen einen gemeinsamen fünften Transistor (T_{10}) enthalten, dessen Steuerelektrode eine Bezugsspannung (V_2) führt, daß die Eingangsschaltung der zweiten Stromspiegelschaltung weiter über die Reihenschaltung aus einer Diode (21) und einem dritten Widerstand (R_3) mit dem Kollektor oder dem Emitter des zu schützenden Transistors (T_1) verbunden ist, und die Ausgangsschaltung der zweiten Stromspiegelschaltung weiter noch mit dem zweiten Widerstand (R_2) in der Ausgangsschaltung der ersten Stromspiegelschaltung verbunden ist. (Fig. 3).

Revendications

1. Circuit de protection servant à protéger un transistor (T_1) contre une surcharge, comprenant

— des premiers moyens (R_1 , 6) pour engendrer un premier signal (I_1) qui constitue une mesure pour le courant de collecteur du transistor (T_1),

— des deuxièmes moyens (9) pour engendrer un deuxième signal (I_2), qui constitue une mesure pour la tension de collecteur-émetteur



du transistor (T_1), ce deuxième signal (I_2) présentant une valeur constante supérieure à celle d'une tension de collecteur-émetteur donnée, qui est indiquée comme tension de coude (V_{KN}) et,

— des troisièmes moyens (14, 15, 16) servant à limiter le courant de collecteur du transistor (T_1) lorsqu'une combinaison des premier (I_1) et deuxième (I_2) signaux dépasse une certaine valeur de seuil (I_D), caractérisé en ce que

— le deuxième signal (I_1) constitue une mesure pour la différence entre la tension de coude (V_{KN}) et la tension de collecteur-émetteur et

— la combinaison des premier (I_1) et deuxième signaux (I_2) est formée par la différence (I_m) entre les premier (I_1) et deuxième signaux (I_2).

2. Circuit de protection selon la revendication 1, caractérisé en ce que les premiers moyens sont munis d'une première résistance (R_1) qui est insérée dans la ligne de collecteur ou d'émetteur du transistor (T_1) et d'un premier convertisseur de courant-tension (6) assurant la conversion de la tension se produisant aux bornes de la première résistance (R_1) en un courant (I_1) proportionnel à ladite tension, que les deuxième moyens sont munis d'un deuxième convertisseur de tension-courant (9) assurant la conversion de la différence entre la tension de collecteur-émetteur et la tension de coude en un courant (I_2) proportionnel à ladite différence et que les troisièmes moyens sont munis d'un amplificateur de commande (16) qui limite le courant traversant le transistor (T_1) de façon que la différence (I_m) entre les courants de sortie des premier (6) et deuxième (9) conver-

tisseurs de tension-courant soit égale à un courant de seuil (I_D) d'une source de courant (14). (Fig. 1).

3. Circuit de protection selon la revendication 2, caractérisé en ce que le premier convertisseur de tension-courant est formé par un premier circuit de miroir de courant comportant un circuit d'entrée, qui est muni d'au moins le montage en série d'une source de courant (20), d'un deuxième transistor (T_2) et d'une première résistance (R_1) et un circuit de sortie qui est muni d'au moins le montage en série d'un troisième transistor (T_4) et d'une deuxième résistance (R_2), que le deuxième convertisseur de tension-courant est formé par un deuxième circuit de miroir de courant comportant un circuit d'entrée qui est muni d'au moins le montage en série d'une source de courant (22) et d'un troisième transistor (T_7) et un circuit de sortie qui est muni d'au moins un quatrième transistor (T_8), les circuits d'entrée et de sortie comportant un cinquième transistor commun (T_{10}), dont l'électrode de commande présente une tension de référence (V_R), que le circuit d'entrée du deuxième circuit de miroir de courant est en outre couplé par l'intermédiaire du montage en série d'une diode (21) et d'une troisième résistance (R_3) au collecteur ou à l'émetteur du transistor à protéger (T_{11}) et que le circuit de sortie du deuxième circuit de miroir de courant est en outre couplé à la deuxième résistance (R_2) dans le circuit de sortie du premier circuit de miroir de courant. (Fig. 3).

