

## Description

The present invention is concerned in general with circuit arrangements which alter the dynamic range of signals, namely compressors which compress the dynamic range and expanders which expand the dynamic range. While the invention is useful for treating various types of signals, including audio signals and video (television) signals, the description of the invention is primarily in the context of the processing of audio signals. The principles of the invention may be applied to the processing of other signals by modifying the disclosed embodiments by applying known techniques. For example, compressors and expanders for video signals can act instantaneously and do not require syllabic control circuitry.

Compressors and expanders are normally used together (a compander system) to effect noise reduction; the signal is compressed before transmission or recording and expanded after reception or playback from the transmission channel. However, compressors may be used alone to reduce the dynamic range, e.g., to suit the capacity of a transmission channel, without subsequent expansion when the compressed signal is adequate for the end purpose. In addition, compressors alone are used in certain products, especially audio products which are intended only to transmit or record compressed broadcast or pre-recorded signals. Expanders alone are used in certain products, especially audio products which are intended only to receive or play back already compressed broadcast or pre-recorded signals. In certain products, a single device is often configured for switchable mode operation as a compressor to record signals and as an expander to play back compressed broadcast or pre-recorded signals.

One long sought after goal in the design of compressors, expanders and companding type noise reduction systems is a high degree of adaptiveness of the compressor and expander to applied signals. That is, the compressor, for example, ideally should provide constant gain throughout its frequency spectrum of operation except at the frequency of a dominant signal component where it would provide dynamic action according to a predetermined compression law. This goal was referred to as "conformal equalization" in U.K. Provisional Specification 43136 filed 11 October 1965 by this inventor. Accordingly, that document (along with two other U.K. Provisional Specifications of this inventor, Nos. 34394 and 02368, filed 11 August 1965 and 18 January 1966, respectively) and subsequent patents derived therefrom (including US-A-3,846,719 and US-A-3,903,485) employed several techniques directed to achieving that goal, including, among others, techniques now common-

ly known as "bandsplitting" and "sliding band".

According to the bandsplitting approach, the spectrum is divided into a plurality of frequency bands, each of which is acted upon independently. In that way a dominant signal component affects dynamic action (compression or expansion) only within a portion of the overall spectrum, in contrast to a wideband approach in which dynamic action throughout the entire spectrum is affected by a dominant signal component. Thus, a bandsplitting system provides a greater degree of adaptiveness or conformance than a wideband system. In theory, a highly adaptive or conformal system could be provided by dividing the overall spectrum into a very large number of frequency bands; however, the complexity and cost of such an arrangement makes it impractical. Consequently, a design compromise is made by selecting a reasonable number of frequency bands capable of providing satisfactory performance. In one well known commercially successful bandsplitting companding type audio noise reduction system (commonly known as A-type noise reduction) four bands are employed ("An Audio Noise Reduction System", by Ray Dolby, J. Audio Eng. Soc., October 1967, Vol. 15, No. 4, pp. 383-388). However, such systems suffer from the same problems as does a wideband noise reduction system, although to a lesser degree because the band is divided up and the problems tend to be confined to the individual bands. These problems are well known in the design of noise reduction systems and include loss of noise reduction effect and the related problems of noise modulation and signal modulation at frequencies not masked by the dominant signal component when a change of gain takes place in response to a dominant signal component. Such problems are chiefly a result of a system failing to be perfectly conformant to the dominant signal. The degree to which such problems are audible also depends on how far the system departs from perfect complementarity. If, for example, the transmission channel response is irregular or unpredictable within the passband of the compressor and expander, then signal modulation effects will not be compensated in the expander.

A dominant signal component is a signal component having a substantial enough level so as to effect dynamic action within the frequency band under consideration. Under complex signal conditions there may be more than one dominant signal component or a dominant signal component and sub-dominant signal components. In a compander system which relies on complementarity of the compressor and expander, all of the signal components must be compressed and expanded in accordance with a defined compression/expansion law in order that the signal spectrum including the

dominant signal component (and other signals affected by dynamic action) can be restored to their correct levels in the expander. This requirement excludes the usefulness in compander systems of various known adaptive and tracking filter techniques and so-called "single ended" noise reduction systems (which operate only on a reproduced signal) in which the filter action is not subject to predetermined compression/expansion laws and whose action may be unpredictable in the presence of multiple signals.

Another approach useful in working toward the goal of increased adaptiveness or conformance is the sliding band technique, which employs signal dependent variable filtering to achieve limiting. Generally, a dominant signal component causes the cutoff or turnover frequency (or frequencies) of one or more variable filters (e.g., high pass, low pass, shelf, notch, etc.) to shift so as to compress or expand the dominant signal component.

A sliding band system operating only in a single high frequency band is described in US-PS Re 28,426 and US-A-4,490,691. This system, which forms the basis for the well known consumer companding type audio noise reduction system known as B-type noise reduction, includes, in a dual path arrangement, a side path having a fixed high pass filter in series with a variable filter.

A "dual path" arrangement is one in which a compression or expansion characteristic is achieved through the use of a main path which is essentially free of dynamic action and one or more secondary or side paths having dynamic action. The side path or paths take their input from the input or output of the main path and their output or outputs are additively or subtractively combined with the main path in order to provide compression or expansion. Generally, a side path provides a type of limiting or variable attenuation and the manner in which it is connected to the main path determines if it boosts (to provide compression) or bucks (to provide expansion) the main path signal components. Such dual path arrangements are described in detail in US-A-3,846,719; US-A-3,903,485; US-A-4,490,691 and US-PS Re 28,426.

A high frequency variable shelving filter in a single path arrangement (e.g., the dynamic action is accomplished in a single signal path) for a companding audio noise reduction system is set forth in US-A-3,911,371. In the embodiments of Figures 1 and 2 of US-A-3,665,345 a dual path arrangement is set forth in which the side path comprises a variable shelving filter having an all-pass characteristic in its quiescent condition. Another approach for providing a variable shelving response for compander systems is set forth in US-A-3,934,190.

One drawback of these sliding band arrange-

ments is that in the presence of a dominant high frequency signal component the variable filter turnover frequency shifts to a frequency above that signal component thereby restricting the frequency area at lower frequencies in which noise reduction is provided. The loss of noise reduction may be more noticeable audibly than in bandsplitting systems and the related side effects (noise modulation and signal modulation) may be more severe than in fixed band arrangements because of a multiplication effect that is inherent in sliding band systems. This effect results from the way in which sliding band systems provide compression. If, for example, there is a dominant high frequency signal and 2 dB of gain reduction is required at that frequency, the variable filter cutoff frequency should shift to the extent necessary to provide that amount of attenuation along the filter slope. However, for lower frequencies, further removed from the new filter cutoff frequency, the effect may be 5 or 10 dB of dynamic action, for example, with a consequent loss of all or most of the noise reduction effect along with possible audible signal or noise modulation. In other words, in this example, a 2 dB change in a dominant signal can cause a 5 or 10 dB change in gain at frequencies removed from the dominant signal. Figure 1 is an idealized compressor characteristic response curve illustrating this effect. (Throughout this document the characteristic response curves illustrated in the various Figures are those of compressors, it being understood that the respective expander characteristic is the complement of the compressor characteristic.) Under relatively rare conditions, when very high frequency dominant signal components (cymbals, for example) control the sliding band filter, there may be audible modulation of non-dominant mid-band signal components that are also present if the expander does not properly track the compressor. This problem is called the "mid-band modulation effect." One approach in solving the problem is set forth in said US-A-4,490,691.

In a fixed band arrangement the same amount of gain reduction would occur throughout the frequency band (whether wide band or one frequency band of a bandsplitting system) in response to a dominant signal component. Thus, while signal or noise modulation may occur, there is no multiplication of the effect: a 2 dB change in the level of a dominant signal component would cause a 2 dB change in gain at frequencies removed from the dominant signal component. However, viewed from the standpoint of noise reduction effect this is a disadvantage of a fixed band arrangement--the full noise reduction effect is not obtained anywhere within the frequency band of operation when limiting occurs in response to a dominant signal component. Figure 2 illustrates this effect. Although it is

not multiplied, there is also the potential for noise and signal modulation throughout the entire frequency band in which the fixed band action occurs.

Despite the disadvantages mentioned, an advantage of a sliding band arrangement is that the full noise reduction effect is obtained at frequencies above the dominant signal component (or below the dominant signal component in the case of a sliding band system acting downward in frequency). Thus an arrangement that achieves the advantages of fixed band and sliding band systems (e.g., the advantage of fixed band is that there is no multiplication of modulation effects and the advantage of sliding band is that there is minimum signal or noise modulation above the dominant signal frequency) without the disadvantages of each (e.g., the disadvantage of fixed band is noise and signal modulation throughout its operating range—although not multiplied and the disadvantage of sliding band is the mid-band modulation effect) would be desirable.

Although it is known to employ fixed band and sliding band actions in separate frequency bands of bandsplitting arrangements and to employ more than one dynamic action within the same frequency band, prior art arrangements have not obtained the above noted advantages of fixed band and sliding band action by employing those actions simultaneously in substantially the same frequency band.

#### Summary of the Invention

The present invention is based on the recognition that the ideal of conformal equalization can be more closely approached by compressor, expander and compander type noise reduction arrangements in which fixed band and sliding band characteristic actions operate within generally the same or overlapping frequency bands. In practice, such a result can be achieved by operating fixed band and sliding band circuit elements in parallel, either as parallel single path devices or as parallel side paths of a dual path arrangement. Such a result can also be achieved by operating such elements in a series arrangement, provided that relatively low compression ratios are used, so that the overall ratio (the product) does not exceed a value suitable for the signal channel. For example, two series elements, each with a ratio of 1.5:1, would yield an overall ratio of 2.25, which is suitable for tape recorder channels. So that the effects of the series connected compressor elements occur in substantially the same dynamic region, the control amplifier gains should be lowered and/or the thresholds of the downstream elements should be raised in order to compensate for the signal gains produced by the upstream elements.

By applying the teachings of the present inven-

tion the advantages of both fixed band and sliding band characteristic actions can be obtained while avoiding their disadvantages. Thus, if a sliding band characteristic and a fixed band characteristic are operable in substantially the same frequency range (wide band or a defined band) and level range, the quiescent characteristic of the combination appears the same as the quiescent characteristic of either one taken alone because the two quiescent characteristics are the same. When a dominant signal component appears within their frequency range each characteristic reacts—the fixed band characteristic drops uniformly in level across the frequency range and the sliding band characteristic slides in frequency.

As these changes occur, the two characteristics, which appeared as one characteristic in the quiescent condition (Figure 3A), are now revealed: the combined characteristic appears as that of a sliding band characteristic above (or below, depending on whether the sliding band acts upwardly or downwardly in frequency) the frequency of the dominant signal and it appears as a fixed band characteristic below (or above) the frequency of the dominant signal. Figure 3B shows an example in which the sliding band is above the dominant signal and Figure 3C shows an example in which the sliding band is below the dominant signal. Two regimes of operation are revealed, divided at the frequency of the dominant signal. Thus, the region which the sliding band characteristic would have left "uncovered" is supplemented by the fixed band characteristic which, in effect, provides a floor or foundation level. The result is to obtain the advantages of both fixed band and sliding band arrangements while avoiding their disadvantages. Maximum noise reduction effect and minimum modulation effects are obtained above (or below) the dominant signal where the sliding band characteristic operates while avoiding the loss of noise reduction and the creation of signal modulation and noise modulation effects below (or above) the dominant signal by the presence of the fixed band characteristic. Thus, there is no multiplication effect below (or above) the dominant frequency as would occur if the sliding band characteristic were operating alone, while obtaining the advantages of the sliding band characteristic above (or below) the dominant frequency.

The characteristics of the example of Figures 3A, 3B and 3C, can be generated by a dual path arrangement having a main path and two side paths: a sliding band side path which has an all pass quiescent characteristic with a single pole high pass or low pass characteristic when active and a wide band fixed band side path. If each side path taken alone is assumed to provide 10 dB of action, then the effect of both side paths summed

together is about 14.5 dB. The quiescent characteristic is thus a flat 14.5 dB wideband. Similar characteristics can be generated by two single side path dual path circuits in series, one circuit having a sliding band side path as just described and the other circuit having a wide band fixed band side path. As a dominant signal appears in either the parallel or series arrangement and the two characteristics react, the area where both characteristics are active (e.g., that area where the sliding band is active) will have a summed characteristic less than the maximum when both characteristics are at their full values (although the sliding band characteristic remains at the 10 dB level where it is effective, the fixed band has attenuated throughout the entire range, thus their sum is less than the former maximum). Note that if two single path parallel elements had been used, the total potential excess effect would be 6 dB instead of only 4.5 dB as in the dual path example. This is a further advantage of dual path circuits over and above those already known.

An even more adaptive arrangement can be achieved according to this invention by providing a bandsplitting arrangement in which the high frequency band and low frequency band are each comprised of series or parallel fixed band/sliding band characteristic action elements. In the high frequency band the sliding band acts upwardly in frequency while in the low frequency band the sliding band acts downwardly in frequency. In the quiescent condition the characteristics overlap so as to provide a flat overall characteristic. By choosing gentle filter slopes (say, 6 dB/octave) and a common quiescent corner frequency in the middle of the frequency band (say, 800 Hz for an audio system), excellent tracking of a dominant signal by both the high and low frequency bands throughout a substantial portion of the band under processing is possible. The quiescent response of such an arrangement is shown in Figure 4A. The presence of two dominant signals results in a fixed band response between the dominant signals and sliding band response at frequencies above and below their frequencies where maximum noise reduction is most critical (Figure 4B).

#### Brief Description of the Drawings

Figure 1 is an idealized compressor characteristic response curve illustrating the prior art sliding band multiplication effect.

Figure 2 is an idealized compressor characteristic response curve illustrating the prior art fixed band limiting effect.

Figure 3A is an idealized compressor characteristic response curve showing the quiescent response of fixed band and sliding band elements

in parallel in accordance with the invention.

Figure 3B is an idealized compressor characteristic response curve showing the response slightly above their thresholds of fixed band and sliding band elements in parallel in accordance with the invention, the sliding band acting upward in frequency.

Figure 3C is an idealized compressor characteristic response curve showing the response slightly above their thresholds of fixed band and sliding band elements in parallel in accordance with the invention, the sliding band acting downward in frequency.

Figure 4A is an idealized compressor characteristic response curve showing the quiescent response of high frequency and low frequency circuits, each having fixed band and sliding band elements in parallel in accordance with the invention, the circuits having a common corner frequency of 800 Hz.

Figure 4B is an idealized compressor characteristic response curve showing the response in the presence of two dominant signals of the same high frequency and low frequency circuits referred to in connection with Figure 4A.

Figure 5 is a block diagram of a prior art sliding band circuit.

Figure 6 is a block diagram of a prior art fixed band circuit.

Figure 7 is a schematic diagram of filters usable in the circuit of Figure 5.

Figure 8 is a schematic diagram of further filters usable in the circuit of Figure 5.

Figure 9 is a schematic diagram of an FET attenuator usable in the circuit of Figure 6.

Figure 10 is a block diagram showing generally the present invention embodied in a companding noise reduction system having parallel fixed band and sliding band elements.

Figure 11 is a block diagram showing a Type I dual path arrangement employing parallel fixed band and sliding band stages of the type described in connection with Figures 5 through 9.

Figure 12 is a block diagram showing a Type II dual path arrangement employing parallel fixed band and sliding band stages of the type described in connection with Figures 5 through 9.

Figure 13 is a block diagram showing a Type I dual path arrangement employing parallel high frequency and low frequency fixed band and sliding band stages of the type described in connection with Figures 5 through 9.

Figure 14 is a block diagram showing generally the present invention embodied in a companding noise reduction system having series fixed band and sliding band elements.

Figure 15 is a block diagram showing a Type I dual path arrangement employing series fixed band

and sliding band stages of the type described in connection with Figures 5 through 9.

Figure 16 is a block diagram showing a Type II dual path arrangement employing series fixed band and sliding band stages of the type described in connection with Figures 5 through 9.

Figure 17 is a block diagram showing a Type I dual path arrangement employing parallel high frequency and low frequency side paths each with fixed band and sliding band stages of the type described in connection with Figures 5 through 9.

Figure 18 is a characteristic response curve relating to the arrangements of Figure 13 and 17.

#### Detailed Description of the Invention

Sliding band and fixed band circuits suitable for use in compressors and expanders are well known, per se, in the art. Figure 5 shows a block diagram of a prior art sliding band circuit for processing audio signals which is usable in several ways: as a single path compressor (as shown), as a single path expander (by placing the circuit in the feed-back loop of an operational amplifier), as a side path of a dual path compressor, or as a side path of a dual path expander. Circuit details of a high frequency sliding band arrangement in accordance with the block diagram of Figure 5 are set forth in US-PS Re 28,426; US-A-4,490,691; and US-A-4,498,060.

Figure 6 shows a block diagram of a prior art fixed band circuit for processing audio signals which is usable in the same ways as a compressor or expander either in a single path arrangement or in a side path of a dual path arrangement. Circuit details of fixed band arrangements in accordance with the block diagram of Figure 6 are set forth in US-A-3,846,719; US-A-3,903,485; and US-A-4,498,060.

The sliding band and fixed band circuit elements useful in the present invention are not limited to the processing of audio signals and include not only circuits of the type just mentioned, but also known modifications of such circuits, such as set forth in US-A-4,490,691, and other known sliding band and fixed band circuits and their equivalents, including, for example, the sliding band arrangements of US-A-3,846,719; US-A-3,903,485; US-A-3,911,371; US-A-3,934,190; US-A-4,306,201; US-A-4,363,006; and US-A-4,363,007, and the fixed band arrangements of US-A-4,306,201 and US-A-4,363,007. The cited patent specifications include details regarding the operation of such circuits as compressors and expanders in dual path arrangements and the operation of compressors as complementary expanders by placing them in the feed-back loop of operational amplifiers.

Referring to Figure 5, the sliding band circuit is

shown having a fixed filter 2, a variable filter 4, an amplifier 6 the output of which is coupled to a non-linear limiter 8 for suppressing overshoots. The output of the overshoot suppression stage provides the circuit output and is also applied to a control circuit having an amplifier 10 the output of which is applied to a half-wave rectifier 12 and integrated by a smoothing filter 14 to provide a control signal for the variable filter 4. The fixed filter 2 may be implemented by a simple single pole RC filter. The variable filter 4 may also be implemented by a simple single pole RC filter in which the source-drain path of a field effect transistor (FET) is operated as a variable resistor by a control voltage applied to the FET gate.

Figure 7 shows a fixed and variable filter arrangement for a high frequency sliding band circuit in which the cutoff frequency of the variable filter 4 moves upward in response to increasing control signal voltage level. Figure 8 shows a fixed and variable filter arrangement for a low frequency sliding band circuit in which the cutoff frequency of the variable filter 4 moves downward in response to increasing control signal voltage level. In Figure 7, the fixed filter is defined by series capacitor 16 and shunt resistor 18 and the variable filter 4 is defined by the parallel arrangement of resistor 20 and capacitor 22 in series and the shunt FET 24 receiving the control signal at its gate. Capacitor 16 and resistor 18 constitute a high pass filter, while resistor 20, capacitor 22 and FET 24 constitute a high pass shelving filter. Although resistor 20 can be omitted (changing variable filter 4 into a variable high pass filter), the inclusion of resistor 20 is useful in avoiding large phase shifts through the filters. In Figure 8, the fixed filter is defined by series inductor 26 and shunt resistor 28 and the variable filter 4 is defined by the parallel arrangement of resistor 30 and inductor 32 in series and the shunt FET 24 receiving the control signal at its base. Inductor 26 and resistor 28 constitute a low pass filter, while resistor 30, inductor 32 and FET 24 constitute a low pass shelving filter. Resistor 30 serves the same purpose as does resistor 20 in the circuit of Figure 7. In practice, inductor 26 and resistor 28 would be replaced by a series resistor and shunt capacitor; non-grounded inductor 32 can be simulated by well known gyrator circuits employing operational amplifiers.

In the arrangements of Figures 7 and 8, under quiescent conditions the FET is pinched off and the variable filter 4 becomes an all pass filter: the fixed filter 2 thus determines the frequency response of the circuit. Under signal conditions as the FET begins to conduct, the variable filter corner frequency rises and when it is above the corner frequency of the fixed filter it determines the frequency response of the circuit. The fixed filter 2 of

the arrangements of Figures 5, 6, 7 and 8 can be omitted if desired, however, the additional sharpness of the overall filter characteristic that occurs when the variable filter corner frequency is near that of the fixed filter is a desirable characteristic.

Returning to the description of Figure 5, the amplifier 10 preferably includes frequency weighting in order to provide increased gain at high frequencies, in the case of a high frequency circuit, or at low frequencies, in the case of a low frequency circuit, in order that the circuit provides sufficient band narrowing (by sliding of the variable filter corner frequency) so as to create the necessary attenuation. The smoothing filter 14 provides the appropriate attack and decay time constants for treating audio signals (e.g., syllabic control).

Referring now to Figure 6, the fixed band circuit is shown having a FET attenuator 36, an amplifier 38 the output of which is coupled to a non-linear limiter 40 for suppressing overshoots. Amplifier 38 and limiter 40 are the same as amplifier 6 and limiter 8 of Figure 5. The output of the overshoot suppression stage provides the circuit output and is also applied to a control circuit having an amplifier 42 the output of which is applied to a phase splitter 44 which drives a full-wave rectifier 46 and is integrated by a smoothing filter 48. Full-wave rectification may also be employed in the sliding band arrangement of Figure 5 and alternatively, the half-wave rectification of Figure 5 may be employed in the fixed band arrangement of Figure 6. Full-wave rectification provides a more accurate control signal but at greater expense. The FET attenuator is configured as a simple voltage divider as shown in Figure 9. The source-drain path of the FET acts as a variable resistor in shunt with series resistor 52. The circuit thus provides wide band variable attenuation. By placing a band defining filter in series with the input before the FET attenuator 36 of Figure 6, the fixed band is effective only within the frequency band defined by the filter.

Figure 10 shows one general arrangement of a compander system in accordance with the parallel aspect of the invention: a fixed band compressor 54 and a sliding band compressor 56 are connected in parallel, each receiving the same input and their respective outputs being combined in summing means 58 for application to a transmission channel. The transmission channel output is applied to a complementary expander in which the compressors 54 and 56 are in the feedback path of a high gain amplifier 60. Providing an expander by such an arrangement is well known. The frequency bands in which the respective fixed band and sliding band compressors operate is substantially the same or at least substantially overlapping. The range of signal levels at which the respective fixed

band and sliding band compressors and expanders provide dynamic action is substantially the same: within a few decibels. The compressors may be any of the devices mentioned above.

The voltage transfer function for a parallel arrangement of compressor or expander elements (e.g., the elements are fed in parallel and their outputs are summed) can be expressed by

$$V_{out} = V_{in}[t_1(s) + t_2(s) + t_3(s) + \dots],$$

where  $V_{in}$  is the applied voltage,  $V_{out}$  is the output voltage, and  $t_1(s)$ ,  $t_2(s)$ , etc. are the transfer functions of each parallel element. The transfer functions add together and each element operates independently.

A more specific arrangement is shown in Figure 11, where the fixed band and sliding band circuits, such as those described in connection with Figures 5 through 9, are located in the side paths of a Type I dual path compander system (of the type generally described in US-A-3,846,719). The arrangement has a compressor 66 in which the input signal is applied to the fixed band stage 68, to the sliding band stage 70, and to the main path 72. The outputs of stages 68 and 70 are combined in summing means 74 and then added to the main path signal components in summing means 76 to provide the compressor output for application to a transmission channel. The side path signal components thus boost the main path signal components causing compressor action. The transmission channel output is applied to the expander 78, configured in a complementary manner to the compressor 66. The expander 78 has an input summing means 80 which receives the transmission channel output and subtracts the sum of the fixed band stage 68 and the sliding band stage 70 outputs, which are added in summing means 82. The side path signal components thus buck the main path signal components causing expander action. The summing means 80 has its output applied to the main path 84 which provides the expander output and the input to the stages 68 and 70.

In Figure 12, a Type II dual path arrangement (of the type generally described in US-A-3,903,485) is shown having a compressor 86 which has an input summing means 88 receiving the input signal and the sum of the fixed band stage 68 and sliding band stage 70 outputs, which are combined in summing means 90. The summing means 88 has its output applied to the main path 92 which provides the compressor output to the transmission channel and the input to the stages 68 and 70 of the compressor. The side path signal components thus boost the main path signal components causing compressor action. The transmission channel output is applied to the expander 94, configured in

a complementary manner to the compressor 86. The input signal is applied to the fixed band stage 68 and the sliding band stage 70 and to the main path 96. The outputs of stages 68 and 70 are summed in summing means 98 and then subtracted from the main path signal components in summing means 100 to provide the expander output. The side path signal components thus buck the main path signal components causing expander action.

As mentioned above, a very useful arrangement is to provide a compressor or expander configured in the nature of bandsplitting high frequency and low frequency bands, each band made up of parallel sliding band and fixed band stages (e.g., a high frequency fixed band stage or element, a high frequency sliding band stage, a low frequency fixed band stage, and a low frequency sliding band stage). The parallel stages can operate as stand alone dynamic range modification devices or as side paths in Type I or Type II dual path arrangements such as described in US-A-3,846,719; US-A-3,903,485; US-PS Re 28,426; and US-A-4,490,691. Preferably, single pole filters with the same corner frequency in each are employed so that the combined quiescent response of the four stages is flat. An advantageous corner frequency for the high and low frequency stages is about 800 Hz for an audio system. With the gently sloping 6 dB/octave slope of the filters, if the high frequency stages have a corner frequency of 800 Hz, significant action as low as 100 or 200 Hz is provided. If the low frequency stage also has a corner frequency of 800 Hz, significant action as high as 6 kHz to 8 kHz is provided. Thus, for signals lying in the range of, say 200 Hz to 6 kHz, which is the band having most of the energy in typical music, the high and low frequency stages are effective and provide a signal tracking effect. For example, as explained further below, for a single dominant signal in that range, the overall response is that of two sliding bands, above and below the dominant signal. For more than one dominant signal the response is a fixed band between the most upper and most lower dominant signals and sliding band responses above and below the most upper and most lower dominant signals, respectively.

Figure 13 shows a bandsplitting arrangement of the type just described. The sliding band stages may be implemented using any of the circuits discussed above. The same corner frequency preferably is used for all of the fixed band and sliding band stages (the quiescent corner frequency in the case of the sliding band stages). The high frequency sliding band stages should operate such that their corner frequency slides upward from the quiescent frequency as signal levels rise. The low frequency sliding band stages should operate such

that their corner frequency slides downward from the quiescent frequency as signal levels rise. Although the arrangement of Figure 13 is shown as a Type I compander, a Type II configuration may also be used. The arrangement has a compressor 102 in which the input signal is applied to the high frequency fixed band stage 104, to the high frequency sliding band stage 106, to the low frequency fixed band stage 108, to the low frequency sliding band stage 110, and to the main path 112. The outputs of stages 104, 106, 108, and 110 are combined in summing means 114 and then added to the main path signal components in summing means 116 to provide the compressor output for application to a transmission channel. The side path signal components thus boost the main path signal components causing compressor action. The transmission channel output is applied to the expander 118, configured in a complementary manner to the compressor 102, which has an input summing means 120 which receives the transmission channel output and subtracts the sum of the high frequency fixed band stage 104, the high frequency sliding band stage 106, the low frequency fixed band stage 108, and the low frequency sliding band stage 110 outputs, which are combined in summing means 122. The side path signal components thus buck the main path signal components causing expander action. The summing means 120 has its output applied to the main path 124 which provides the expander output and the input to the stages 104, 106, 108, and 110.

Figure 14 shows one general arrangement of a compander system in accordance with the series aspect of the invention: a fixed band compressor 130 and a sliding band compressor 132 are connected in series, the fixed band compressor receiving the input and their overall compressor output being taken from the sliding band compressor 132 for application to a transmission channel. The transmission channel output is applied to a complementary sliding band expander 134 in series with a complementary fixed band expander 136. The system output is taken from the output of expander 136. The frequency bands in which the respective fixed band and sliding band compressors and expanders operate is substantially the same or at least substantially overlapping. The signal levels at which the respective fixed band and sliding band compressors and expanders provide dynamic action is substantially the same. The compressors and complementary expanders may be any of the devices mentioned above.

The voltage transfer function for a series arrangement of compressor or expander elements can be expressed by

$$V_{out} = V_{in}[t_1(s)t_2(s)t_3(s)\dots],$$

where  $V_{in}$  is the applied voltage,  $V_{out}$  is the output voltage, and  $t_1(s)$ ,  $t_2(s)$ , etc. are the transfer functions of each series element. The transfer functions multiply times each other.

A more specific arrangement is shown in Figure 15, where the fixed band and sliding band circuits, such as those described in connection with Figures 5 through 9, are located in the side paths of series Type I dual path compressors and expanders in a compander system (of the type generally described in US-PS 3,846,719). The arrangement has a fixed band compressor 138 in which the input signal is applied to the fixed band stage 140 and to the main path 142. The output of stage 140 is then added to the main path signal components in summing means 144 to provide the fixed band compressor output for application to the sliding band compressor 146. The latter has a sliding band stage 148 and a main path 150, which both receive the output of the fixed band compressor. The output of stage 148 is added to the main path signal components in summing means 152 to provide the overall compressor output to a transmission channel. The side path signal components in each compressor boost the main path signal components causing compressor action. The transmission channel output is applied to the expander portion of the compander system, including a complementary sliding band expander 154 in series with a complementary fixed band expander 156. Expander 154 has an input summing means 158 that receives the transmission channel output and subtracts the output of the sliding band stage 148. Expander 156 likewise has an input summing means 160 that receives the output of the sliding band expander 154 and subtracts the output of fixed band stage 140. The side path signal components thus buck the main path signal components causing expander action. Note that the series order of the expanders is complementary to the order of the compressors.

In Figure 16, a series Type II dual path compander arrangement (of the type generally described in US-PS 3,903,485) is shown, also employing fixed band and sliding band circuits, such as those described in connection with Figures 5 through 9, in the side paths series. The arrangement has a fixed band compressor 162 in which the input signal is applied to an input summing means 164 that also receives the output of the fixed band stage 140 and combines the applied signal components. The summing means 164 has its output applied to the main path 166 which provides the fixed band compressor output to the sliding band compressor 168. The latter has an input summing means 170 which combines the output of compressor 162 with the output of the

sliding band stage 148. The summing means 170 has its output applied to the main path 172 which provides the input to the sliding band stage 148 and the overall compressor output to the transmission channel. The side path signal components in each compressor boost the main path signal components causing compressor action. The transmission channel output is applied to the expander portion of the compander system, including a complementary sliding band expander 174 in series with a complementary fixed band expander 176. The input to expander 174 is applied to the sliding band stage 148 and the main path 176. The output of sliding band stage 148 is subtracted from the main path in summing means 178 which provides the output to the fixed band expander 178. The input to expander 178 is applied to fixed band stage 140 and to the main path 180. The output of the fixed band stage 140 is subtracted from the main path in summing means 182 to provide the overall system output. The side path signal components buck the main path signal components causing expander action. Note that the series order of the expanders is also complementary to the order of the compressors in this arrangement.

As mentioned above, a very useful arrangement is to provide a compressor or expander configured in the nature of bandsplitting high frequency and low frequency bands, each band made up of series sliding band and fixed band stages of the type described in connection with Figures 5 through 9. The series high frequency and low frequency stages are arranged in two parallel paths that can operate as stand alone dynamic range modification devices or as side paths in Type I or Type II dual path arrangements such as described in US-A-3,846,719; US-A-3,903,485; US-PS Re 28,426; and US-A-4,490,691. Preferably, single pole filters with the same corner frequency in each are employed so that the combined quiescent response of the stages is flat. An advantageous corner frequency for the high and low frequency stages is about 800 Hz for an audio system. With the gently sloping 6 dB/octave slope of the filters, if the high frequency stages have a corner frequency of 800 Hz, significant action as low as 100 or 200 Hz is provided. If the low frequency stage also has a corner frequency of 800 Hz, significant action as high as 6 kHz to 8 kHz is provided. Thus, for signals lying in the range of, say 200 Hz to 6 kHz, which is the band having most of the energy in typical music, the high and low frequency stages are effective and provide a signal tracking effect. For example, as explained further below, for a single dominant signal in that range, the overall response is that of two sliding bands, above and below the dominant signal. For more than one dominant signal the response is a fixed band be-

tween the most upper and most lower dominant signals and sliding band responses above and below the most upper and most lower dominant signals, respectively.

Figure 17 shows a bandsplitting arrangement of the type just described. The sliding band stages may be implemented using any of the circuits discussed above. The same corner frequency preferably is used for all of the fixed band and sliding band stages (the quiescent corner frequency in the case of the sliding band stages). The high frequency sliding band stages should operate such that their corner frequency slides upward from the quiescent frequency as signal levels rise. The low frequency sliding band stages should operate such that their corner frequency slides downward from the quiescent frequency as signal levels rise.

Figure 17 has a compressor 184 in which the input signal is applied to a main path 186 and to two parallel side paths: a high frequency side path having in series a high frequency fixed band stage 188 and a high frequency sliding band stage 190; and a low frequency side path having a low frequency fixed band stage 192 and a low frequency sliding band stage 194. The outputs of the two side paths are combined in summing means 196 and then added to the main path signal components in summing means 198 to provide the compressor output for application to a transmission channel. The side path signal components thus boost the main path signal components causing compressor action. The transmission channel output is applied to the expander 200, configured in a complementary manner to the compressor 184, which has an input combining means 202 which receives the transmission channel output and subtracts therefrom the sum of the high frequency and low frequency side paths. Combining means 202 feeds the main path 204 from which the overall system output is taken and the side path inputs are taken to the series high frequency fixed band and sliding band stages 188 and 190 and to the series low frequency fixed band and sliding band stages 192 and 194. The side path outputs are combined in summing means 206 before application to the input combining means 202. The side path signal components buck the main path signal components causing expander action. Although the arrangement of Figure 17 is shown as a Type I compander, a Type II configuration may also be used.

In Figures 11 through 17 the main path of each compressor and expander is linear with respect to dynamic range and the level of the sum of the side path stages is generally less than the maximum level of the main path. The transmission channel in those Figures may include any type of storage or transmission medium and may also include means for converting or encoding the analog signal com-

ponents from the compressor into a different form (digital, for example), the storage or transmission of the encoded signals, and means for re-converting or decoding the encoded signals back into analog signal components. The order of the series fixed band and sliding band compressors may be as shown in Figures 14 through 17, or, alternatively, the sliding band compressor may be located upstream of the fixed band compressor. For complementarity, the expander circuits are arranged in reverse order to the arrangement of the compressor circuits in the arrangements of Figures 14 through 17. So that the effects of the series connected compressor elements occur in substantially the same dynamic region, the control amplifier gains should be lowered and/or the thresholds of the downstream elements should be raised in order to compensate for the signal gains produced by the upstream elements. In the expander portion of the system, the control amplifier gains should be raised and/or the thresholds of the upstream elements should be lowered.

Figure 18 is a representation of the quiescent characteristics of the compressor 102 of the arrangement of Figure 13 and of the compressor 184 of the arrangement of Figure 17. A common corner frequency of 800 Hz for all four stages is assumed. The curves also illustrate the substantial overlap of the 6 dB/octave skirts of the single pole filters.

### Claims

1. A circuit for modifying the dynamic range of an input signal, comprising
  - fixed band variable gain circuit means (54),
  - sliding band circuit means (56),
  - said fixed band variable gain circuit means and sliding band circuit means operating at least partially within the same frequency and level region,
  - means for connecting said circuit means in series or parallel,
  - means for coupling the input signal to the series or parallel arrangement of said circuit means, and
  - means for deriving an output signal from the series or parallel arrangement of said circuit means.
2. A circuit according to claim 1, wherein at least one of said circuit means (54, 56) operates in a restricted frequency band, and the circuit means operate at least partially within the same frequency range under quiescent conditions.
3. A circuit according to claim 1 or 2, wherein the

tween the most upper and most lower dominant signals and sliding band responses above and below the most upper and most lower dominant signals, respectively.

Figure 17 shows a bandsplitting arrangement of the type just described. The sliding band stages may be implemented using any of the circuits discussed above. The same corner frequency preferably is used for all of the fixed band and sliding band stages (the quiescent corner frequency in the case of the sliding band stages). The high frequency sliding band stages should operate such that their corner frequency slides upward from the quiescent frequency as signal levels rise. The low frequency sliding band stages should operate such that their corner frequency slides downward from the quiescent frequency as signal levels rise.

Figure 17 has a compressor 184 in which the input signal is applied to a main path 186 and to two parallel side paths: a high frequency side path having in series a high frequency fixed band stage 188 and a high frequency sliding band stage 190; and a low frequency side path having a low frequency fixed band stage 192 and a low frequency sliding band stage 194. The outputs of the two side paths are combined in summing means 196 and then added to the main path signal components in summing means 198 to provide the compressor output for application to a transmission channel. The side path signal components thus boost the main path signal components causing compressor action. The transmission channel output is applied to the expander 200, configured in a complementary manner to the compressor 184, which has an input combining means 202 which receives the transmission channel output and subtracts therefrom the sum of the high frequency and low frequency side paths. Combining means 202 feeds the main path 204 from which the overall system output is taken and the side path inputs are taken to the series high frequency fixed band and sliding band stages 188 and 190 and to the series low frequency fixed band and sliding band stages 192 and 194. The side path outputs are combined in summing means 206 before application to the input combining means 202. The side path signal components buck the main path signal components causing expander action. Although the arrangement of Figure 17 is shown as a Type I compander, a Type II configuration may also be used.

In Figures 11 through 17 the main path of each compressor and expander is linear with respect to dynamic range and the level of the sum of the side path stages is generally less than the maximum level of the main path. The transmission channel in those Figures may include any type of storage or transmission medium and may also include means for converting or encoding the analog signal com-

ponents from the compressor into a different form (digital, for example), the storage or transmission of the encoded signals, and means for re-converting or decoding the encoded signals back into analog signal components. The order of the series fixed band and sliding band compressors may be as shown in Figures 14 through 17, or, alternatively, the sliding band compressor may be located upstream of the fixed band compressor. For complementarity, the expander circuits are arranged in reverse order to the arrangement of the compressor circuits in the arrangements of Figures 14 through 17. So that the effects of the series connected compressor elements occur in substantially the same dynamic region, the control amplifier gains should be lowered and/or the thresholds of the downstream elements should be raised in order to compensate for the signal gains produced by the upstream elements. In the expander portion of the system, the control amplifier gains should be raised and/or the thresholds of the upstream elements should be lowered.

Figure 18 is a representation of the quiescent characteristics of the compressor 102 of the arrangement of Figure 13 and of the compressor 184 of the arrangement of Figure 17. A common corner frequency of 800 Hz for all four stages is assumed. The curves also illustrate the substantial overlap of the 6 dB/octave skirts of the single pole filters.

## Claims

1. A circuit for modifying the dynamic range of an input signal, comprising  
fixed band variable gain circuit means (54),  
sliding band circuit means (56),  
said fixed band variable gain circuit means and sliding band circuit means operating at least partially within the same frequency and level region,  
means for connecting said circuit means in series or parallel,  
means for coupling the input signal to the series or parallel arrangement of said circuit means, and  
means for deriving an output signal from the series or parallel arrangement of said circuit means.
2. A circuit according to claim 1, wherein at least one of said circuit means (54, 56) operates in a restricted frequency band, and the circuit means operate at least partially within the same frequency range under quiescent conditions.
3. A circuit according to claim 1 or 2, wherein the



circuit means (54, 56) are arranged in parallel circuit paths.

4. A circuit according to claim 1 or 2, wherein the circuit means (130, 132; 134, 136) are arranged in a series path.

5. A circuit according to any of the preceding claims, wherein said fixed band variable gain circuit means includes first and second fixed band variable gain circuits (108, 104), each having a band defining filter, the filters having a substantially identical cutoff frequency, the band defining filter included with said first fixed band variable gain circuit (108) defining a band in the lower portion of the frequency spectrum of the input signal and the band defining filter included with said second fixed band variable gain circuit (104) defining a band in the upper portion of the frequency spectrum of the input signal, and wherein said sliding band circuit means includes first and second sliding band circuits (110, 106), the quiescent filter characteristic of said first sliding band circuit (110) defining a band substantially the same as that defined by the band defining filter of said first fixed band variable gain circuit (108), the quiescent filter characteristic of said second sliding band circuit (106) defining a band substantially the same as that defined by the band defining filter of said second fixed band variable gain circuit (104), the first sliding band circuit having a cutoff frequency that shifts downward in frequency, and the second sliding band circuit having a cutoff frequency that shifts upward in frequency.

6. The circuit of claim 3, wherein the fixed band variable gain circuit means and the sliding band circuit means have voltage transfer functions  $t_1(s)$  and  $t_2(s)$ , respectively, and the parallel arrangement of the circuit means has a transfer function such that when input signal components are applied, represented by the voltage  $V_{in}$ , the output voltage  $V_{out}$  is represented by

$$V_{out} = V_{in}[t_1(s) + t_2(s)].$$

7. The circuit of claim 4, wherein the fixed band variable gain circuit means and the sliding band circuit means have voltage transfer functions  $t_1(s)$  and  $t_2(s)$ , respectively, and the series arrangement of the circuit means has a transfer function such that when input signal components are applied, represented by the voltage  $V_{in}$ , the output voltage  $V_{out}$  is represented by

$$V_{out} = V_{in}[t_1(s)t_2(s)].$$

8. A method for modifying the dynamic range of input signal components within a frequency band, comprising

selecting two circuit characteristic actions represented by the voltage transfer functions  $t_1(s)$  and  $t_2(s)$ , wherein one of the transfer functions represents a fixed band variable gain characteristic and the other transfer function represents a sliding band characteristic, the characteristic actions operating at least partially within substantially the same frequency and level region, and

operating the circuit characteristics such that when input signal components are applied, represented by the voltage  $V_{in}$ , the output voltage  $V_{out}$  is represented by

$$V_{out} = V_{in}[t_1(s) + t_2(s)].$$

9. A method for modifying the dynamic range of input signal components within a frequency band, comprising

selecting two circuit characteristic actions represented by the voltage transfer functions  $t_1(s)$  and  $t_2(s)$ , wherein one of the transfer functions represents a fixed band variable gain characteristic and the other transfer function represents a sliding band characteristic, the characteristic actions operating at least partially within substantially the same frequency and level region, and

operating the circuit characteristics such that when input signal components are applied, represented by the voltage  $V_{in}$ , the output voltage  $V_{out}$  is represented by

$$V_{out} = V_{in}[t_1(s)t_2(s)].$$

#### Patentansprüche

- Schaltung zur Modifizierung des Dynamikbereiches eines Eingangssignals, umfassend eine Festbandschaltungsanordnung (54) mit variabler Verstärkung, eine Gleitbandschaltungsanordnung (56), wobei die Festbandschaltungsanordnung mit variabler Verstärkung und die Gleitbandschaltungsanordnung wenigstens teilweise innerhalb des gleichen Frequenz- und Pegelbereiches arbeiten, eine Einrichtung zur Verbindung der Schaltungsanordnungen in Reihe oder parallel, eine Einrichtung zum Einleiten des Eingangssignals in die Reihen- oder Parallelanordnung der Schaltungsanordnungen und



eine Einrichtung zur Ableitung eines Ausgangssignals von der Reihen- oder Parallelanordnung der Schaltungsanordnungen.

3. Schaltung nach Anspruch 1, bei der wenigstens eine der Schaltungsanordnungen (54,56) in einem begrenzten Frequenzband arbeitet und die Schaltungsanordnungen im Ruhezustand wenigstens teilweise innerhalb des gleichen Frequenzbereiches arbeiten.
4. Schaltung nach Anspruch 1 oder 2, bei der die Schaltungsanordnungen (54,56) in parallelen Schaltungswegen angeordnet sind.
5. Schaltung nach Anspruch 1 oder 2, bei der die Schaltungsanordnungen (130,132;134,136) in einem Reihenzug angeordnet sind.
6. Schaltung nach einem der vorhergehenden Ansprüche, bei der die Festbandschaltungsanordnung mit variabler Verstärkung eine erste und eine zweite Festbandschaltung (108,104) mit variabler Verstärkung einschließt, von denen jede ein bandbestimmendes Filter aufweist, die Filter eine im wesentlichen identische Eckfrequenz aufweisen, das bandbestimmende Filter, das in der ersten Festbandspaltung (108) mit variabler Verstärkung enthalten ist, ein Band im unteren Teil des Frequenzspektrums des Eingangssignals festlegt und das Band bestimmende Filter, das in der zweiten Festbandschaltung mit variabler Verstärkung enthalten ist, ein Band in dem oberen Teil des Frequenzspektrums des Eingangssignals festlegt, und bei der die Gleitbandschaltungsanordnung eine erste und eine zweite Gleitbandschaltung (110,106) einschließt, die Ruhefilterkennlinie der ersten Gleitbandschaltung (110) ein Band festlegt, das im wesentlichen das gleiche wie das ist, das von dem bandbestimmenden Filter der ersten Festbandschaltung (108) mit variabler Verstärkung festgelegt wird, die Ruhefilterkennlinie der zweiten Gleitbandschaltung (108) ein Band festlegt, das im wesentlichen das gleiche ist, wie dasjenige, das das bandbestimmende Filter der zweiten Festbandspaltung (104) mit variabler Verstärkung festlegt, die erste Gleitbandschaltung eine Eckfrequenz aufweist, die sich frequenzmäßig nach unten verschiebt, und die zweite Gleitbandschaltung eine Eckfrequenz aufweist, die sich frequenzmäßig nach oben verschiebt.
7. Schaltung nach Anspruch 3, bei der die Festbandschaltungsanordnung mit variabler Verstärkung und die Gleitbandschaltungsanordnung Spannungsübertragungsfunktionen  $t_1(s)$

bzw.  $t_2(s)$  aufweisen und die Parallelanordnung der Schaltungsanordnungen eine solche Übertragungsfunktion aufweist, daß, wenn Eingangssignalkomponenten angelegt werden, die durch die Spannung  $V_{in}$  repräsentiert werden, die Ausgangsspannung  $V_{out}$  repräsentiert wird

$$V_{out} = V_{in} [t_1(s) + t_2(s)].$$

7. Schaltung nach Anspruch 4, bei der die Festbandschaltungsanordnung mit variabler Verstärkung und die Gleitbandschaltungsanordnung Spannungsübertragungsfunktionen  $t_1(s)$  bzw.  $t_2(s)$  aufweisen und die Reihenanzahl der Spaltungsanordnungen eine solche Übertragungsfunktion aufweist, daß, wenn Eingangssignalkomponenten angelegt werden, die durch die Spannung  $V_{in}$  repräsentiert werden, die Ausgangsspannung  $V_{out}$  repräsentiert wird durch

$$V_{out} = V_{in} [t_1(s) t_2(s)].$$

8. Verfahren zur Modifizierung des Dynamikbereiches von Eingangssignalkomponenten innerhalb eines Frequenzbandes, umfassend

Auswählen von zwei charakteristischen Schaltungsaktionen die durch die Spannungsübertragungsfunktionen  $t_1(s)$  und  $t_2(s)$  repräsentiert werden, wobei eine der Übertragungsfunktionen eine Festbandkennlinie mit variabler Verstärkung repräsentiert und die andere Übertragungsfunktion eine Gleitbandkennlinie repräsentiert und die charakteristischen Aktionen wenigstens teilweise innerhalb im wesentlichen desselben Frequenz- und Pegelbereiches arbeiten, und Betreiben der Schaltungskennlinien in einer solchen Weise, daß, wenn Eingangssignalkomponenten angelegt werden, die durch die Spannung  $V_{in}$  repräsentiert werden, die Ausgangsspannung  $V_{out}$  repräsentiert wird durch

$$V_{out} = V_{in} [t_1(s) + t_2(s)].$$

9. Verfahren zur Modifizierung des Dynamikbereiches von Eingangssignalkomponenten innerhalb eines Frequenzbandes, umfassend

Auswählen von zwei charakteristischen Schaltungsaktionen, die durch die Spannungsübertragungsfunktionen  $t_1(s)$  und  $t_2(s)$  repräsentiert werden, wobei eine der Übertragungsfunktionen eine Festbandkennlinie mit variabler Verstärkung repräsentiert und die andere Übertragungsfunktion eine Gleitbandkennlinie repräsentiert und die charakteristischen Aktionen wenigstens teilweise innerhalb im wesentlichen des gleichen Frequenz- und Pegelbereiches



ches arbeiten, und

Betreiben der Schaltungskennlinien in einer solchen Weise, daß, wenn Eingangssignalkomponenten angelegt werden, die durch die Spannung  $V_{in}$  repräsentiert werden, die Ausgangsspannung  $V_{out}$  repräsentiert wird durch

$$V_{out} = V_{in} [t_1(s) t_2(s)].$$

## Revendications

1. Circuit pour la modification de l'intervalle dynamique d'un signal d'entrée comprenant :

- un circuit à gain variable et à bande fixe (54);
- un circuit à bande mobile (56);

ledit circuit à gain variable et à bande fixe et ledit circuit à bande mobile fonctionnant au moins partiellement à la même fréquence et au même niveau,

- un moyen pour le raccordement dudit circuit en série ou en parallèle;
- un moyen de couplage du signal d'entrée au montage en série ou en parallèle dudit circuit et
- un moyen de dérivation d'un signal de sortie à partir du montage en série ou en parallèle dudit circuit.

2. Circuit selon la revendication 1, dans lequel au moins un desdits circuits (54, 56) fonctionne dans une bande de fréquences restreinte et le circuit fonctionne au moins partiellement dans le même intervalle de fréquences sous conditions au repos.

3. Circuit selon la revendication 1 ou 2, dans lequel les circuits (54, 56) sont placés selon des montages de circuits parallèles.

4. Circuit selon la revendication 1 ou 2, dans lequel les circuits (130, 132; 134, 136) sont montés en série.

5. Circuit selon l'une quelconque des revendications précédentes, dans lequel ledit circuit à gain variable et à bande fixe comprend des premier et second circuits à gain variable et à bande fixe (108, 104) possédant chacun un filtre de définition de bande, les filtres possédant une fréquence de coupure pratiquement identique, le filtre de définition de bande inclus dans ledit premier circuit à gain variable et à bande fixe (108) définissant une bande dans la partie inférieure du spectre de fréquences du signal d'entrée et le filtre de définition de bande inclus dans ledit second circuit à gain variable et à bande fixe définissant une bande dans

la partie supérieure du spectre de fréquences du signal d'entrée et dans lequel ledit circuit à bande mobile comprend des premier et second circuits à bande mobile (110, 106), la caractéristique au repos du filtre dudit premier circuit à bande mobile (110) définissant une bande pratiquement identique à celle définie par le filtre de définition de bande dudit premier circuit à gain variable et à bande fixe (108), la caractéristique au repos du filtre dudit second circuit à bande mobile (106) définissant une bande pratiquement identique à celle définie par le filtre de définition de bande dudit second circuit à gain variable et à bande fixe (104), le premier circuit à bande mobile possédant une fréquence de coupure se décalant vers le bas et le second circuit à bande mobile possédant une fréquence de coupure se décalant vers le haut.

6. Circuit selon la revendication 3, dans lequel le circuit à gain variable et à bande fixe et le circuit à bande mobile possèdent des fonctions respectives de transfert de tension  $t_1(s)$  et  $t_2(s)$  et le montage en parallèle des circuits possède une fonction de transfert de telle façon que, lorsqu'on applique les composantes du signal d'entrée représentées par la tension  $V_{in}$ , la tension de sortie  $V_{out}$  est représentée par la formule suivante :

$$V_{out} = V_{in} [t_1(s) + t_2(s)].$$

7. Circuit selon la revendication 4, dans lequel le circuit à gain variable et à bande fixe et le circuit à bande mobile comprennent des fonctions respectives de transfert de tension  $t_1(s)$  et  $t_2(s)$  et le montage en série des circuits possède une fonction de transfert telle que, lorsque l'on applique les composantes du signal d'entrée représentées par la tension  $V_{in}$ , la tension de sortie  $V_{out}$  est représentée par la formule suivante :

$$V_{out} = V_{in} [t_1(s) \cdot t_2(s)].$$

8. Procédé de modification de l'intervalle dynamique des composantes d'un signal d'entrée dans une bande de fréquences comprenant :

- la sélection de deux mises en fonction de caractéristique de circuit représentées par les fonctions de transfert de tension  $t_1(s)$  et  $t_2(s)$  parmi lesquelles une des fonctions de transfert représente une caractéristique de gain variable à bande fixe et l'autre fonction de transfert représente une caractéristique de bande mobile, les mises en fonction de caractéris-



tique fonctionnant au moins partiellement à la même fréquence et au même niveau et

- l'activation des caractéristiques de circuit telles que, lorsqu'on applique les composantes du signal d'entrée représentées par la tension  $V_{in}$ , la tension de sortie  $V_{out}$  est représentée par la formule suivante :

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$$V_{out} = V_{in}[t_1(s) + t_2(s)].$$

9. Procédé de modification de l'intervalle dynamique des composantes d'un signal d'entrée dans une bande de fréquences comprenant :

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- la sélection de deux mises en fonction de caractéristique de circuit représentées par les fonctions de transfert de tension  $t_1(s)$  et  $t_2(s)$  parmi lesquelles une des fonction de transfert représente une caractéristique de gain variable à bande fixe et l'autre fonction de transfert représente une caractéristique de bande mobile, les mises en fonction de caractéristique fonctionnant au moins partiellement à la même fréquence et au même niveau et

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- l'activation des caractéristiques de circuit telles que, lorsqu'on applique les composantes du signal d'entrée représentées par la tension  $V_{in}$ , la tension de sortie  $V_{out}$  est représentée par la formule suivante :

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$$V_{out} = V_{in}[t_1(s).t_2(s)].$$

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