

Description

The invention relates to an over-voltage protection circuit, e.g. for a television apparatus power supply.

The horizontal deflection circuit in some conventional television receivers encompasses an output stage that includes a horizontal deflection winding and a trace capacitance that supplies deflection current to the deflection winding during each trace interval. A retrace capacitance is coupled across the deflection winding during the retrace interval. Energy is replenished during retrace via a flyback transformer. A deflection transistor switch, that is conductive during trace, causes a DC voltage B+ to be developed across a primary winding of the flyback transformer during trace.

Aspects of the invention are specified in the claims.

In a circuit embodying the invention, a secondary winding of the flyback transformer is series coupled through a rectifier arrangement to a common conductor, referred to as ground. The rectifier arrangement includes a diode switch. The anode of the diode is at, for example, ground potential. The cathode of the diode switch is coupled to one end terminal of the secondary winding. A filter capacitor is coupled between ground and a second end terminal of the secondary winding that is remote from the cathode of the diode switch. A load circuit is coupled across the filter capacitor.

During trace, a trace voltage developed in the secondary winding produces a trace current in the secondary winding that is coupled to the filter capacitor and to the load circuit. The secondary winding current develops a rectified DC output supply voltage in the filter capacitor. The secondary winding current flows in a current path that includes the diode switch. The secondary winding current produces a forward current in the diode switch that causes the diode switch to be conductive during trace. When the diode switch is conductive, the secondary winding forms a voltage source having a relatively low output impedance. As long as the diode switch is conductive, the forward voltage developed at the cathode of the diode switch is negligible. Therefore, the output supply voltage is determined mainly by the primary-to-secondary turn ratio of the flyback transformer and by voltage B+, and is not affected by the voltage at the cathode of diode switch.

During retrace, a retrace pulse voltage is developed in the secondary winding of the transformer in the opposite polarity that causes the diode switch to be nonconductive. A retrace voltage is developed at the cathode of the diode switch. Thus, in normal operation, the diode switch is conductive throughout trace and nonconductive during

retrace, so as to provide the DC output supply voltage that is rectified by the diode switch.

In a well known side pincushion distortion correction circuit of the diode modulator type, the same diode switch that was discussed before also provides switching operation in the diode modulator. To that end, a circuit branch of the diode modulator has an end terminal that is coupled between the secondary winding and the cathode of the diode switch, such that the cathode forms a three way junction node where three branches intersect: the circuit branch of the diode modulator, a circuit branch that includes the diode switch and a circuit branch that includes the secondary winding. A current flowing through the above mentioned circuit branch of the diode modulator, during, for example, the first half of trace, may supply a portion of the current that flows in the secondary winding and, hence reduce the forward current in the diode switch. Thus, the secondary winding current may be equal to the sum of the absolute value of the forward current and the current in the circuit branch of the diode modulator.

The current in the secondary winding is determined by the load current. Therefore, a decrease in the load current causes the forward current in the diode switch to decrease. The load circuit that is coupled across the filter capacitor associated with the diode switch may include a vertical amplifier integrated circuit of the television receiver that is energized by the output supply voltage. During degaussing, and during operation of the service switch, when the vertical raster is collapsed, or in the event of a fault condition, for example, the vertical amplifier output current, hence the load current, may be significantly smaller than during normal operation. Should the load current decrease, the secondary winding current would also decrease. Should the secondary winding current decrease to a level that is, for example, equal to that of the current in the circuit branch of the diode modulator, the current in the circuit branch of the diode modulator will cause the forward current of the diode switch to become zero. A further decrease in the secondary winding current will cause the cathode voltage of the diode switch that is then nonconductive to increase substantially above ground potential.

The trace voltage that is developed across the secondary winding is coupled in series with the voltage at the cathode of the diode switch. An increase in the cathode voltage during trace, disadvantageously, may cause the output supply voltage to exceed its normal operation level. An increase in the output supply voltage may damage other integrated circuits such as, for example, audio processing integrated circuits that are also energized by the output supply voltage.

A television apparatus power supply embodying the invention includes a controllable switch coupled to a horizontal deflection winding for producing a horizontal deflection current in the horizontal deflection winding, and an output supply voltage. A raster distortion correction circuit is coupled to the horizontal deflection winding for producing a modulation of the horizontal deflection current. The raster distortion correction circuit produces a second current. A vertical deflection circuit is coupled to the output supply voltage that produces a load current in the vertical deflection circuit for energizing the vertical deflection circuit. The load current has a magnitude that is within a predetermined range of values during normal operation and outside the range of values when the vertical deflection circuit is disabled or when a fault condition occurs. A first control signal is generated that is indicative when the magnitude of the load current is outside the range of values. The control signal is coupled to the raster distortion correction circuit for disabling the operation of the raster distortion correction circuit when the magnitude of the load current is outside the range of values.

In accordance with an embodiment of the invention, the control signal prevents the second current from causing an increase in the output supply voltage.

In the Drawing:

The sole FIGURE illustrates an East-west raster distortion correction circuit of a horizontal deflection circuit that includes a protection circuit, embodying an aspect of the invention.

The sole FIGURE illustrates a horizontal deflection circuit output stage 100 that operates also as a power supply for generating a supply voltage V. Voltage V of, for example, +26 volts, is developed across a filter capacitor C5. Voltage V energizes a load circuit 40a and a vertical deflection amplifier 40b. Load circuit 40a may be, for example, an audio processing stage of a television receiver, not shown.

Output stage 100 includes a deflection switching transistor Q1 that is antiparallel coupled with a damper diode D1. A retrace capacitor C2 is coupled across diode D1 and between the collector and emitter electrodes of transistor Q1. A primary winding W1 of a flyback transformer T1 is coupled between an input supply voltage B+ and the collector electrode of transistor Q1. A horizontal deflection winding L_y , a linearity inductor L_{LIN} , a primary winding T2a of a transformer T2 of an East-west pincushion distortion correction circuit 30 and a trace capacitor C1 form a series arrangement that is coupled between the collector of transistor Q1 and hot ground. Transistor Q1 is switched at a

horizontal rate in accordance with a drive signal H, that is developed at its base electrode. Signal H_r is produced in a horizontal oscillator and driver stage 150 in a well known manner. The switching operation of transistor Q1 produces a horizontal deflection current i_y in a well known manner.

A secondary winding W2 of flyback transformer T1 has a first end terminal W2b that is coupled to filter capacitor C5 where voltage V is developed. A second end terminal W2a of winding W2 is coupled via a rectifier arrangement 70 to chassis ground. Rectifier arrangement 70 includes diodes CR01 and CR02 that are coupled in series with winding W2. The anode of diode CR02, operating as a diode switch, is at chassis ground potential. The cathode of diode CR02 is coupled to the anode of diode CR01 via a terminal 32. Diode CR01 is coupled between terminal 32 and terminal W2a of winding W2.

During trace, when transistor Q1 (or diode D1) is conductive, a trace voltage that is approximately equal to voltage B+ is developed in winding W1 of flyback transformer T1. During trace, a voltage V_{W2} , forming a trace portion of an AC voltage, is developed by transformer action across winding W2 in the polarity shown. As a result of rectifier arrangement 70, voltage V_{W2} produces a half wave rectified current i_{W2} in winding W2 that is coupled to filter capacitor C5 and to circuits 40a and 40b.

In normal operation, during trace, current i_{W2} flows in a current path that includes forward biased diodes CR01 and CR02. Consequently, voltage V, that is developed at terminal W2b, is equal to the value of voltage B+ multiplied by the turns ratio between windings W2 and W1. During retrace, when transistor Q1 is nonconductive, a relatively high retrace voltage of the opposite polarity is developed across winding W1. A retrace pulse voltage is developed in winding W2 of the opposite polarity to the polarity during trace, that causes diodes CR01 and CR02 to operate as a nonconductive switch. Thus, in normal operation, diodes CR01 and CR02 are conductive throughout trace and nonconductive during retrace.

A secondary winding T2b of transformer T2, of pincushion distortion correction circuit 30, has a first end terminal 31 that is coupled to a modulation voltage developing capacitor C3. Terminal 32, that is coupled between diodes CR02 and CR01, forms a second end terminal of winding T2b.

During horizontal trace, a trace voltage developed across trace capacitor C1 produces, by transformer action of transformer T2, a trace voltage V_{T2b} across winding T2b in the polarity shown. Voltage V_{T2b} is applied in series with capacitor C3 for producing a voltage V_m developed in capacitor C3 in the polarity shown by the arrow, and for producing an oscillatory current i_{T2b} .

During horizontal retrace, diodes CR01 and CR02 become nonconductive, as explained before. Consequently, a retrace voltage that is developed in winding T2b causes current i_{T2b} in winding T2b to reverse its direction and to flow in the direction shown by the arrow, at the end of retrace and during the first half of trace. Also, a retrace voltage is developed at terminal 32 that is coupled between diodes CR01 and CR02. During the second half of trace, trace current i_{T2b} flows in the opposite direction to that of the arrow.

A control circuit 30a of pincushion distortion correction circuit 30 is coupled to end terminal 31 of capacitor C3. Control circuit 30a generates, in a manner that is later described, a modulation sink current i_m having a controllable average value that controls voltage V_m in capacitor C3 in accordance with the average DC component of current i_m . When the average value of sink current i_m is, for example, zero, voltage V_m is at a maximum. On the other hand, when the average value of current i_m is at a maximum, voltage V_m is at a minimum.

Modulation voltage V_m , as controlled by control circuit 30a, establishes by the transformer action of transformer T2, the level of voltage V_{T2a} across primary winding T2a of transformer T2. Thus, voltage V_{T2a} is modulated in accordance with voltage V_m or current i_m . Voltage V_{T2a} is applied in a direction that causes the trace voltage across deflection winding L_y to be smaller than voltage V_{C1} , developed across trace capacitor C1.

When the average value of current i_m is at a minimum, voltage V_m is at a maximum, and voltage V_{T2a} is at a maximum. Voltage V_{T2a} at the maximum causes the amplitude of deflection current i_y to be at a minimum. On the other hand, when the average value of current i_m is at a maximum, voltage V_m is at a minimum and the amplitude of deflection current i_y is at a maximum.

Control circuit 30a, that produces sink current i_m , includes transistors Q2, Q3, Q4, Q5 and Q6 that form a switched amplifier. Transistors Q2 and Q3 form an input, differential stage of the switched amplifier. The base of transistor Q3 forms a noninverting input terminal of the switched amplifier. A reference level V_{ref} developed at the base of transistor Q3 is produced in a zener diode Z. The base of transistor Q2 forms an inverting input terminal of the switched amplifier. The collector of transistor Q3 is coupled to a load resistor R10 and to the base of transistor Q4. The emitter of transistor Q4 is coupled to the base of switching transistor Q6 in a Darlington configuration. The emitter of transistor Q6 is coupled to chassis ground. The collector of transistor Q6 is coupled via an inductor L_m to capacitor C3. The collector of transistor Q6 forms a switching output terminal of the switched amplifier for producing sink current i_m in inductor L_m that

provides East-West pincushion distortion correction.

A horizontal retrace pulse signal is coupled from a winding W3 of flyback transformer T1 via a series arrangement of a capacitor C7 and a resistor R13 to the base of transistor Q2. During horizontal retrace, the retrace pulse signal in winding W3 produces an upramping portion UR of a sawtooth signal V_{INV} developed at the base of transistor Q2. During horizontal trace, a downramping portion DR of signal V_{INV} changes at a smaller rate than upramping portion UR. During an interval having a controllable length that includes a portion of upramping portion UR and an immediately following portion of downramping portion DR, signal V_{INV} is more positive than voltage V_{ref} developed at the base of transistor Q3. Assuming a zero offset voltage, as long as the base voltage of transistor Q2 is more positive than that of transistor Q3, transistor Q6 operates as a switch that is turned on. Conductive transistor Q6 couples inductor L_m across capacitor C3 to produce an upramping portion of sink current i_m in inductor L_m . After transistor Q6 is turned off during trace, sink current i_m continues flowing, as a result of the magnetic energy stored in inductor L_m , in a current path that includes a diode D2. Diode D2 is coupled between the collector of transistor Q6 and voltage V. The length of the interval when transistor Q6 is conductive is modulated by, for example, a parabola voltage V_p that varies in a vertical rate parabolic manner.

Voltage V_p is coupled to the base of transistor Q2 via an R-C network 50. Network 50 includes a potentiometer 50a that is adjustable for controlling the amplitude of the vertical parabola voltage developed at the base of transistor Q2. Network 50 includes also an integrating capacitor 50b that determines the slope of the corresponding portions of sawtooth signal V_{INV} . Voltage V_p causes the average DC value of signal V_{INV} at the base of transistor Q2 to vary in a vertical rate parabolic manner. The result is that the length of the interval when transistor Q6 is conductive, hence each of voltage V_m and the average value of current i_m , varies in a vertical rate parabolic manner.

A resistor R141 is coupled between the collector of transistor Q6 and the base of transistor Q2. Resistor R141 produces a negative feedback current having, during a given horizontal period H, a DC or average value that is proportional to voltage V_m . The current in resistor R141 is coupled to integrating capacitor 50b. As a result of the negative feedback, voltage V_m , that is controlled in a closed loop, varies in a parabolic manner.

Voltage V_p is produced in a vertical deflection circuit 60 that includes vertical amplifier 40b of the type LA7831 produced by Sanyo, for example. A series arrangement that includes a vertical deflec-

tion winding L_v , a sampling resistor R_v and a DC blocking capacitor C8 is coupled between an output terminal of amplifier 40a and chassis ground. Parabola voltage V_p is developed across capacitor C8 in a well known manner.

Vertical deflection circuit 60 includes a vertical control circuit 61 that produces an input signal 61a having a sawtooth waveform that is coupled to an input terminal 40b2 of amplifier 40b. Vertical control circuit 61 is responsive to a control signal SERVICE/DEGAUSSING that is used for disabling the generation of a vertical deflection current i_v in winding L_v during, for example, operation of a service switch and degaussing. An example of a vertical deflection circuit that includes an amplifier of the type LA7831 and a service mode operation feature is described in U.S. Patent 4,694,226 in the name of James A. Wilber, entitled VERTICAL DEFLECTION CIRCUIT WITH SERVICE MODE OPERATION.

As a result of parabola voltage V_p , the instant within horizontal retrace when transistor Q6 becomes conductive occurs earlier at the center of vertical trace than at the top and bottom. Hence, each of the average value of current i_m that sinks charge from capacitor C3 in each horizontal period H, and the level of voltage V_m , is at a maximum at the center of vertical trace and at a minimum at the top and bottom of vertical trace. Consequently, the amplitude of deflection current i_v is at a maximum at the center of vertical trace and at a minimum at the top and bottom, in a manner that provides East-West pincushion distortion correction. A potentiometer R14, that is coupled to the base of transistor Q2, provides width adjustment.

When, during horizontal trace, transistor Q2 becomes nonconductive, the collector voltage of transistor Q2 increases. Consequently, transistor Q5, having a base electrode that is coupled to the collector of transistor Q2, becomes conductive. When transistor Q5 becomes conductive, it forms a low impedance between the base and emitter of transistor Q6 that, advantageously, speeds up the turn-off of transistor Q6.

Transformers T1 and T2 electrically isolate, with respect to electrical shock hazard, voltage V and control circuit 30a from voltage B+ and from AC mains supply voltage V_{AC} . Voltage B+ is electrically nonisolated with respect to electrical hazard, from AC mains supply voltage V_{AC} that is used for producing voltage B+. Thus transformers T1 and T2 provide an isolation barrier. Supply voltage V is coupled via a resistor R15 to a supply terminal 40b1 of vertical amplifier 40b.

During, for example, degaussing, it may be desirable to disable the vertical deflection current in order to prevent introducing purity error in a cathode ray tube of the receiver, not shown. Thus,

during degaussing and also during operation of a service switch, signal SERVICE/DEGAUSSING is generated in a well known manner, not shown, for disabling the generation of the vertical deflection current i_v . When signal SERVICE/DEGAUSSING is generated, or during the occurrence of a fault condition, a supply current i_{40b} flowing in vertical deflection amplifier 40b and through resistor R15 may be at a substantially smaller magnitude than during normal operation. The result is that trace current i_{W2} in winding W2 will also decrease.

Assume that throughout the first half of normal horizontal trace operation, current i_{W2} is larger than current i_{T2b} . Therefore, diode CR02 that conducts the difference between currents i_{W2} and i_{T2b} remains conductive throughout horizontal trace. It follows that, during normal operation, diode CR02 prevents trace current i_{T2b} from affecting voltage V.

Should current i_{W2} decrease significantly relative to its normal operation level, as a result of the aforementioned decrease in load current i_{40b} , positive trace current i_{T2b} in winding T2b of transformer T2 might become equal to current i_{W2} , during a significant portion of the first half of the horizontal trace. Therefore, diode CR02 might become nonconductive during such significant portion of the first half of horizontal trace. The result is that current i_{T2b} might produce a wide pulse of voltage V_{32} at the cathode of reverse-biased diode CR02 having a relatively large positive peak level. The sum of voltages V_{W2} and V_{32} forms voltage V. Therefore, should the peak level of the pulse of voltage V_{32} become large and its width significant, during the aforementioned vertical raster collapse, voltage V_{32} would cause voltage V to be larger than during normal operation. Voltage V might harm some integrated circuits depicted as load 40a that are energized by supply voltage V.

In an illustrative implementation of the invention, a transistor Q7 has an emitter electrode and a base electrode that are coupled to end terminals of resistor R15, respectively, for sensing load current i_{40b} in vertical amplifier 40b. The collector of transistor Q7 is coupled via a parallel arrangement of a filter capacitor C9 and a bleeder resistor R16 to ground. A switch diode D3 is coupled between the base of transistor Q2 and a junction terminal that is coupled between the collector of transistor Q7 and the parallel arrangement of filter capacitor C9 and resistor R16.

During normal operation, supply or load current i_{40b} in vertical amplifier 40b that flows also in resistor R15 produces a voltage drop across resistor R15 that is sufficiently large to cause transistor Q7 to be conductive during at least a portion of each vertical deflection cycle. Consequently, a DC positive filtered voltage that is developed across capacitor C9 is maintained sufficiently high to main-

tain diode D3 back-biased throughout each vertical deflection cycle.

Should the maximum value of load current i_{40b} in a given vertical deflection cycle become smaller than a predetermined level, as a result of, for example, vertical deflection circuit 60 being disabled, transistor Q7 would remain turned-off. Therefore diode D3 would become conductive throughout each vertical deflection cycle. Consequently, the base voltage of transistor Q2 would become smaller than that of transistor Q3. The result is that transistor Q6 would be maintained nonconductive indefinitely, causing the average value current i_m to be zero.

When the average value of current i_m is at a maximum, voltage V_m is at a minimum and the positive peak amplitude of current i_{T2b} in winding T2b, at the beginning of trace, is at a maximum. Conversely, when the average value of current i_m is at a minimum, the peak positive amplitude of current i_{T2b} is at a minimum.

When, for example, the vertical raster is collapsed, current i_m is zero because of the operation of diode D3 that was explained above. The result is that current i_{T2b} is at a minimum positive peak amplitude that is smaller than current i_{W2} flowing in winding W2. Since the difference between current i_{W2} and current i_{T2b} flows as the forward current of diode CR02, diode CR02 remains conductive throughout the first half of horizontal trace. It follows that voltage V_{32} is maintained at the forward voltage level of diode CR02 throughout horizontal trace. When diode CR02 is conductive, diode CR02 advantageously prevents current i_{T2b} from affecting current i_{W2} . Thus, diode CR02 decouples a current path that includes winding T2b from a current path that includes winding W2. In this way, advantageously, voltage V is prevented from exceeding its normal operation level when, for example, the vertical raster is collapsed.

When vertical amplifier 40b is disabled during, for example, operation of a service switch, voltage V will continue to be generated for enabling horizontal scanning operation. Such normal horizontal scanning operation may be required during operation of the service switch. Thus, voltage V is protected by the operation of transistor Q7 in a way that, advantageously, does not necessitate a complete shutdown of horizontal deflection circuit output stage 100.

Claims

1. A power supply apparatus for a television display, comprising:
 - a vertical deflection circuit (40b);
 - means (R15) for generating a control signal (61a) indicative of disablement of normal

operation of said vertical deflection circuit;

a horizontal deflection circuit (100) for producing a horizontal deflection current (i_y) in a horizontal deflection winding (L_y);

a side pincushion distortion correction circuit (30) coupled to said horizontal deflection circuit (100) for producing a modulation of said horizontal deflection current (i_y); characterized by

means (Q7,D3,Q2) responsive to said control signal (61a) and coupled to said pincushion distortion correction circuit (30) for disabling said pincushion distortion correction circuit (30) when normal operation of said vertical deflection circuit (40b) is disabled.

2. A power supply apparatus according to Claim 1 wherein said horizontal deflection circuit (100) comprises a horizontal flyback transformer (T1) having first (W1) and second (W2) windings and a horizontal deflection switch (Q1) operating at a horizontal deflection frequency and coupled to said first winding (W1) of said transformer (T1) for generating an AC supply voltage (V_{W2}) in said second winding (W2) at a horizontal deflection frequency, characterized by a diode switch (70) coupled to said second winding (W2) for rectifying said AC supply voltage (W2) to produce an output supply current (i_{W2}) that is coupled to said vertical deflection circuit (40b) for energizing said vertical deflection circuit, said supply current (i_{W2}) being coupled via said second winding (W2) to said diode switch (70) to produce a forward current in said diode switch that causes said diode switch to be conductive during a horizontal trace interval and nonconductive during a horizontal retrace interval such that when said vertical deflection circuit (40b) is disabled, a magnitude of said supply current (i_{W2}) becomes substantially smaller than during normal operation, wherein said pincushion distortion correction circuit (30) comprises a second transformer (T2) having a first winding (T2a) that is coupled to said deflection winding (L_y) and having a second winding (T2b) that is coupled to said diode switch (70) such that the switching operation of said diode switch also produces an oscillatory second current (i_{T2b}) in said second winding (T2b) of said second transformer (T2), said second current (i_{T2b}) being combined in said diode switch (70) with said supply current (i_{W2}) that flows in said second winding (W2) of said flyback transformer (T1) in a manner that reduces said forward current in said diode switch during said trace interval and wherein said pincushion distortion correction circuit disabling means



tain diode D3 back-biased throughout each vertical deflection cycle.

Should the maximum value of load current i_{40b} in a given vertical deflection cycle become smaller than a predetermined level, as a result of, for example, vertical deflection circuit 60 being disabled, transistor Q7 would remain turned-off. Therefore diode D3 would become conductive throughout each vertical deflection cycle. Consequently, the base voltage of transistor Q2 would become smaller than that of transistor Q3. The result is that transistor Q6 would be maintained nonconductive indefinitely, causing the average value current i_m to be zero.

When the average value of current i_m is at a maximum, voltage V_m is at a minimum and the positive peak amplitude of current i_{T2b} in winding T2b, at the beginning of trace, is at a maximum. Conversely, when the average value of current i_m is at a minimum, the peak positive amplitude of current i_{T2b} is at a minimum.

When, for example, the vertical raster is collapsed, current i_m is zero because of the operation of diode D3 that was explained above. The result is that current i_{T2b} is at a minimum positive peak amplitude that is smaller than current i_{W2} flowing in winding W2. Since the difference between current i_{W2} and current i_{T2b} flows as the forward current of diode CR02, diode CR02 remains conductive throughout the first half of horizontal trace. It follows that voltage V_{32} is maintained at the forward voltage level of diode CR02 throughout horizontal trace. When diode CR02 is conductive, diode CR02 advantageously prevents current i_{T2b} from affecting current i_{W2} . Thus, diode CR02 decouples a current path that includes winding T2b from a current path that includes winding W2. In this way, advantageously, voltage V is prevented from exceeding its normal operation level when, for example, the vertical raster is collapsed.

When vertical amplifier 40b is disabled during, for example, operation of a service switch, voltage V will continue to be generated for enabling horizontal scanning operation. Such normal horizontal scanning operation may be required during operation of the service switch. Thus, voltage V is protected by the operation of transistor Q7 in a way that, advantageously, does not necessitate a complete shutdown of horizontal deflection circuit output stage 100.

Claims

1. A power supply apparatus for a television display, comprising:
 - a vertical deflection circuit (40b);
 - means (R15) for generating a control signal (61a) indicative of disablement of normal

operation of said vertical deflection circuit;

a horizontal deflection circuit (100) for producing a horizontal deflection current (i_y) in a horizontal deflection winding (L_y);

a side pincushion distortion correction circuit (30) coupled to said horizontal deflection circuit (100) for producing a modulation of said horizontal deflection current (i_y); characterized by

means (Q7,D3,Q2) responsive to said control signal (61a) and coupled to said pincushion distortion correction circuit (30) for disabling said pincushion distortion correction circuit (30) when normal operation of said vertical deflection circuit (40b) is disabled.

2. A power supply apparatus according to Claim 1 wherein said horizontal deflection circuit (100) comprises a horizontal flyback transformer (T1) having first (W1) and second (W2) windings and a horizontal deflection switch (Q1) operating at a horizontal deflection frequency and coupled to said first winding (W1) of said transformer (T1) for generating an AC supply voltage (V_{W2}) in said second winding (W2) at a horizontal deflection frequency, characterized by a diode switch (70) coupled to said second winding (W2) for rectifying said AC supply voltage (W2) to produce an output supply current (i_{W2}) that is coupled to said vertical deflection circuit (40b) for energizing said vertical deflection circuit, said supply current (i_{W2}) being coupled via said second winding (W2) to said diode switch (70) to produce a forward current in said diode switch that causes said diode switch to be conductive during a horizontal trace interval and nonconductive during a horizontal retrace interval such that when said vertical deflection circuit (40b) is disabled, a magnitude of said supply current (i_{W2}) becomes substantially smaller than during normal operation, wherein said pincushion distortion correction circuit (30) comprises a second transformer (T2) having a first winding (T2a) that is coupled to said deflection winding (L_y) and having a second winding (T2b) that is coupled to said diode switch (70) such that the switching operation of said diode switch also produces an oscillatory second current (i_{T2b}) in said second winding (T2b) of said second transformer (T2), said second current (i_{T2b}) being combined in said diode switch (70) with said supply current (i_{W2}) that flows in said second winding (W2) of said flyback transformer (T1) in a manner that reduces said forward current in said diode switch during said trace interval and wherein said pincushion distortion correction circuit disabling means



(Q7,D3,Q2) decreases the magnitude of said second current (i_{T2b}) in said second winding (T2b) of said second transformer (T2) when the magnitude of said output supply current (i_{W2}) is substantially smaller than during normal operation to prevent said second current (i_{T2b}) from back-biasing said diode switch (70) at least substantially throughout said horizontal trace interval.

Patentansprüche

1. Stromversorgungsvorrichtung für eine Fernseh-anzeige, umfassend:

eine Vertikal-Ablenkschaltung (40b);

Mittel (R15) zur Erzeugung eines Steuersignals (61a), das die Unwirksamkeit des normalen Betriebes der Vertikal-Ablenkschaltung anzeigt;

eine Horizontal-Ablenkschaltung (100) zur Erzeugung eines Horizontal-Ablenkstroms (i_y) in einer Horizontal-Ablenkwicklung (L_y);

eine Seiten-Kissenverzeichnungs-Korrekturschaltung (30), die mit der Horizontal-Ablenkschaltung (100) verbunden ist, um eine Modulation des Horizontal-Ablenkstroms (i_y) zu erzeugen, gekennzeichnet durch:

Mittel (Q7, D3, Q2), die auf das Steuersignal (61a) ansprechen und mit der Kissenverzeichnungs-Korrekturschaltung (30) verbunden sind, um die Kissenverzeichnungs-Korrekturschaltung (30) unwirksam zu machen, wenn der normale Betrieb der Vertikal-Ablenkschaltung (40b) unwirksam ist.

2. Stromversorgungsvorrichtung nach Anspruch 1, bei der die Horizontal-Ablenkschaltung (100) einen Horizontal-Zeilenendwandler (T1), eine erste Wicklung (W1) und eine zweite Wicklung (W2) sowie einen Horizontal-Ablenkschalter (Q1) enthält, der mit einer Horizontal-Ablenfrequenz arbeitet und mit der ersten Wicklung (W1) des Wandlers (T1) verbunden ist, um eine Wechselstrom-Versorgungsspannung (V_{W2}) in der zweiten Wicklung (W2) mit einer Horizontal-Ablenfrequenz zu erzeugen, gekennzeichnet durch einen Diodenschalter (70), der mit der zweiten Wicklung (W2) verbunden ist, um die Wechselstrom-Versorgungsspannung (V_{W2}) gleichzurichten und einen Ausgangs-Versorgungsstrom (i_{W2}) zu erzeugen, der der Vertikal-Ablenkschaltung (40b) zur Speisung der Vertikal-Ablenkschaltung zugeführt wird, wobei der Versorgungsstrom (i_{W2}) über die zweite Wicklung (W2) dem Diodenschalter (70) zugeführt wird, um in dem Diodenschalter einen Strom in Durchlaßrichtung zu erzeugen, der bewirkt, daß der Diodenschal-

ter während des Horizontal-Hinlaufintervalls leitend und während des Horizontal-Rücklaufintervalls nicht leitend wird, so daß bei Unwirksamkeit der Vertikal-Ablenkschaltung (40b) die Größe des Versorgungsstroms (i_{W2}) nennenswert kleiner als bei normalen Betrieb wird, wobei die Kissenverzeichnungs-Korrekturschaltung (30) einen zweiten Wandler (T2) mit einer ersten Wicklung (T2a), die mit der Ablenkwicklung (L_y) verbunden ist und mit einer zweiten Wicklung (T2b), die mit dem Diodenschalter (70) verbunden ist, umfaßt, so daß der Schaltbetrieb des Diodenschalters auch einen oszillierenden zweiten Strom (i_{T2b}) in der zweiten Wicklung (T2b) des zweiten Wandlers (T2) erzeugt, wobei der zweite Strom (i_{T2b}) in dem Diodenschalter (70) mit dem in der zweiten Wicklung (W2) des Zeilenendwandlers (T1) fließende Versorgungsstrom (i_{T2b}) in einer Weise kombiniert wird, daß der Strom in Durchlaßrichtung in dem Diodenschalter während des Hinlaufintervalls vermindert wird, und wobei die Mittel (Q7, D3, Q2) zum Unwirksammachen der Kissenverzeichnungs-Korrekturschaltung die Größe des zweiten Stroms (i_{T2b}) in der zweiten Wicklung (T2b) des zweiten Wandlers (T2) verringern, wenn die Größe des Ausgangs-Versorgungsstroms (i_{W2}) nennenswert kleiner als während des normalen Betriebes ist, um den zweiten Strom (i_{T2b}) daran zu hindern, den Diodenschalter (70) wenigstens weitgehend während des ganzen Horizontal-Hinlaufintervalls in Sperr-Richtung vorzuspannen.

Revendications

1. Dispositif d'alimentation d'énergie pour un système d'affichage de télévision comprenant :
un circuit de déviation verticale (40b) ;
des moyens (R15) pour générer un signal de commande (61a) indiquant une désactivation du fonctionnement normal dudit circuit de déviation verticale ;
un circuit de déviation horizontale (100) pour produire un courant de déviation horizontale (i_y) dans un enroulement de déviation horizontale (L_y) ;
un circuit de correction de distorsion en coussin latéral (30) couplé audit Circuit de déviation horizontale (100) pour produire une modulation dudit courant de déviation horizontale (i_y), caractérisé par :
des moyens (Q7, D3, Q2) agissant en réponse audit signal de commande (61a) et couplés audit circuit de correction de distorsion en coussin (30) pour désactiver ledit circuit de correction de distorsion en coussin (30) lorsque le fonctionnement normal dudit circuit de



déviatioti verticale (40b) est désactivé.

2. Dispositif d'alimentation en énergie selon la revendication 1 dans lequel ledit circuit de déviation horizontale (100) comprend un transformateur de retour du balayage horizontal (T1) comportant des premier (W1) et second (W2) enroulements et un commutateur de déviation horizontale (Q1) fonctionnant à une fréquence de déviation horizontale et qui est couplé audit premier enroulement (W1) dudit transformateur (T1) pour générer une tension d'alimentation (V_2) en courant alternatif dans ledit second enroulement (W2) à une fréquence de déviation horizontale, caractérisé par un commutateur à diode (70) couplé audit second enroulement (W2) pour redresser ladite tension d'alimentation (V_{W2}) en courant alternatif, afin de produire un courant d'alimentation de sortie (i_{W2}) qui est couplé audit circuit de déviation verticale (40b) pour exciter ce circuit de déviation verticale, ledit courant d'alimentation (i_{W2}) étant couplé, par l'intermédiaire dudit second enroulement (W2) audit commutateur à diode (70) pour produire un courant de conduction dans ledit commutateur à diode qui amène ce commutateur à diode à être conducteur pendant un intervalle de tracé horizontal et non conducteur durant un intervalle de retour horizontal, de manière que lorsque ledit circuit de déviation verticale (40b) est désactivé, une amplitude dudit courant d'alimentation (i_{W2}) devient sensiblement plus petite que lors d'un fonctionnement normal, dans lequel ledit circuit de correction de distorsion en coussin (30) comprend un second transformateur (T2) ayant un premier enroulement (T2a) qui est couplé audit enroulement de déviation (L_y) et comportant un second enroulement (T2B) qui est couplé audit commutateur à diode (70) de manière que le fonctionnement de commutation dudit commutateur à diode produise également un second courant oscillatoire (i_{T2b}) dans ledit second enroulement (T2b) dudit second transformateur (T2), ledit second courant (i_{T2b}) étant combiné dans ledit transformateur à diode (70) avec ledit courant d'alimentation (i_{W2}) qui circule dans ledit second enroulement (W2) dudit transformateur de retour de balayage (T1) d'une manière qui réduit ledit courant de conduction dans ledit commutateur à diode, durant ledit intervalle de tracé et dans lequel lesdits moyens désactivant le circuit de correction de distorsion en coussin (Q7, D3, Q2) diminuent l'amplitude dudit second courant (i_{T2b}) dans ledit second enroulement (T2b) dudit second transformateur (T2) lorsque l'amplitude dudit courant d'alimentation de sortie (i_{W2})

est sensiblement plus petit que lors du fonctionnement normal afin d'empêcher ledit second courant (i_{T2b}) de polariser en retour ledit commutateur à diode (70) au moins sensiblement durant l'intervalle de tracé horizontal.