

RADIO-FREQUENCY TRANSMITTER, SUCH AS FOR BROADCASTING AND CELLULAR BASE STATIONS

CROSS-REFERENCE TO RELATED APPLICATIONS

The subject matter of this application is related to that of U.S. Patent Application No. 13/228063, by Igor Acimovic, attorney docket reference 810317-US-NP, filed on the same date as the present application, and entitled "RADIO-FREQUENCY CIRCUIT HAVING A TRANSCOUPING ELEMENT," which is incorporated herein by reference in its entirety.

BACKGROUND

Field of the Invention

The present invention relates to equipment for telecommunication systems and, more specifically but not exclusively, to radio-frequency (RF) transmitters and power amplifiers, and passive RF circuits suitable for use therein.

Description of the Related Art

This section introduces aspects that may help facilitate a better understanding of the invention(s). Accordingly, the statements of this section are to be read in this light and are not to be understood as admissions about what is in the prior art or what is not in the prior art.

A recent trend in the telecommunications industry includes the introduction of wideband digital-modulation systems, such as the third generation (3G) cellular-system wideband code-division-multiple-access (WCDMA) and the fourth generation (4G) cellular-system orthogonal frequency-division multiple-access (OFDMA). This trend has had a profound effect on power-amplifier specifications because an RF power amplifier used in a wideband digital-modulation system needs to properly and efficiently handle a signal that has a fast-changing envelope, a high peak-to-average power ratio (PAPR), and a bandwidth that can be tens of megahertz. In addition, for cost reasons, a single power amplifier is usually configured to amplify multiple modulated carriers.

A typical RF power amplifier is inherently nonlinear, with its gain being a function of the output-power level. The gain usually decreases when the output power approaches the saturation level of the amplifier, and the phase of the gain can either increase or decrease, depending on the type of the active medium. Amplitude and/or phase distortions in the power amplifier tend to cause the generation of spurious spectral components often referred to as inter-modulation-distortion (IMD) products. IMD products are detrimental, for example, because they increase the level of interference between adjacent RF channels.

SUMMARY

Disclosed herein are various embodiments of a transmitter that uses a digital pre-distortion (DPD) circuit to mitigate the effects of nonlinearity of a multistage or multi-branch power amplifier, such as a Doherty power amplifier or a Chireix power amplifier. The DPD circuit relies on two or more feedback signals received from an RF-output circuit of the transmitter to generate individually pre-distorted signals for each stage/branch of the power amplifier. The use of these individually pre-distorted signals advantageously enables the transmitter to achieve a more efficient suppression of inter-modulation-distortion products than that typically achieved with a comparable prior-art transmitter.

According to one embodiment, provided is an apparatus having: a digital pre-distortion circuit configured to pre-distort a digital input signal to generate a first pre-distorted digital signal and a second pre-distorted digital signal different from the first pre-distorted signal; a first amplifier branch configured to generate a first amplified signal based on the first pre-distorted digital signal; a second amplifier branch configured to generate a second amplified signal based on the second pre-distorted digital signal; and a radio-frequency (RF) circuit configured to combine the first and second amplified signals to generate a combined signal. The RF circuit is further configured to generate first and second feedback signals based on at least two of the first amplified signal, the second amplified signal, and the combined signal. The digital pre-distortion circuit is configured to generate the first pre-distorted digital signal and the second pre-distorted digital signal based on said first and second feedback signals to counteract nonlinearity in the first and second amplifier branches.

According to another embodiment, provided is a signal-amplification method having the steps of: pre-distorting a digital input signal to generate a first pre-distorted digital signal and a second pre-distorted digital signal different from the first pre-distorted signal; generating a first amplified signal based on the first pre-distorted digital signal in a first amplifier branch; generating a second amplified signal based on the second pre-distorted digital signal in a second amplifier branch; combining the first and second amplified signals in a radio-frequency (RF) circuit to generate a combined signal; and generating first and second feedback signals based on at least two of the first amplified signal, the second amplified signal, and the combined signal. The step of pre-distorting comprises the sub-step of generating the first pre-distorted digital signal and the second pre-distorted digital signal based on said first and second feedback signals to counteract nonlinearity in the first and second amplifier branches.

According to yet another embodiment, provided is an apparatus having: means for pre-distorting a digital input signal to generate a first pre-distorted digital signal and a second pre-distorted digital signal different from the first pre-distorted signal; a first amplifier branch configured to generate a first amplified signal based on the first pre-distorted digital signal; a second amplifier branch configured to generate a second amplified signal based on the second pre-distorted digital signal; means for combining the first and second amplified signals to generate a combined signal; and means for generating first and second feedback signals based on at least two of the first amplified signal, the second amplified signal, and the combined signal. The means for pre-distorting is configured to generate the first pre-distorted digital signal and the second pre-distorted digital signal based on said first and second feedback signals to counteract nonlinearity in the first and second amplifier branches.

BRIEF DESCRIPTION OF THE DRAWINGS

Other aspects, features, and benefits of various embodiments of the invention will become more fully apparent, by way of example, from the following detailed description and the accompanying drawings, in which:

FIG. 1 shows a block diagram of a radio-frequency (RF) transmitter according to one embodiment of the invention;

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FIG. 2 shows a block diagram of a transceiver that can be used in the RF transmitter of FIG. 1 according to one embodiment of the invention;

FIG. 3 shows a circuit diagram of an RF circuit that can be used in the RF transmitter of FIG. 1 according to one embodiment of the invention;

FIG. 4 shows a circuit diagram of an RF circuit that can be used in the RF transmitter of FIG. 1 according to another embodiment of the invention; and

FIG. 5 shows a top view of a microstrip circuit that can be used to implement the RF circuit of FIG. 4 according to one embodiment of the invention; and

FIG. 6 shows a circuit diagram of a two-stage amplifier according to one embodiment of the invention.

DETAILED DESCRIPTION

One method that can be used to linearize the nonlinear response of a radio-frequency (RF) power amplifier over its intended dynamic range is digital pre-distortion (DPD). DPD works in the digital domain and uses digital-signal-processing techniques to pre-distort a baseband signal before modulation, up-conversion, and amplification. With DPD, the power amplifier can be utilized substantially up to its saturation point while maintaining a sufficiently accurate linear relationship between the input and output signals. DPD is an attractive technique, e.g., because it can significantly increase the power efficiency of a power amplifier and be implemented using standard and/or inexpensive circuit components. A high degree of flexibility can be achieved if programmable hardware is used, such as digital signal processors (DSPs) and/or field-programmable gate arrays (FPGAs). In addition, DPD does not require significant changes in the schematics of the costly analog part (e.g., the RF-output circuit) of the corresponding transmitter and lends itself to various advantageous implementations in which the analog front end of the transmitter has a relatively small size, and the configurable digital part of the transmitter can be placed very close to the antenna.

FIG. 1 shows a block diagram of an RF transmitter **100** according to one embodiment of the invention. Transmitter **100** uses a Doherty amplification scheme to convert a digital input signal **102** into an analog RF-output signal **152**. Output signal **152** is applied to an output load (e.g., an antenna) **160**. A feedback path

comprising a feedback-receiver (FBR) circuit **120** and a DPD circuit **110** enables transmitter **100** to apply digital pre-distortion to input signal **102**, thereby suppressing IMD products in output signal **152**.

The Doherty amplification scheme of transmitter **100** employs power amplifiers **140₁** and **140₂** connected in parallel as indicated in FIG. 1. Output signals **142₁** and **142₂** generated by amplifiers **140₁** and **140₂**, respectively, are combined in an RF-output circuit **150** as further described below in reference to FIGs. 3-4 to produce output signal **152**. Amplifier **140₁** is configured to operate, e.g., as a class-B or a class-AB amplifier and is also referred to as a primary or carrier stage. Amplifier **140₂** is configured to operate, e.g., as a class-C amplifier and is also referred to as an auxiliary or peak stage. A brief description of operating configurations corresponding to the pertinent amplifier classes can be found, e.g., in U.S. Patent Nos. 7,498,876 and 7,928,799, both of which are incorporated herein by reference in their entirety.

Due to different configurations of amplifiers **140₁** and **140₂**, only amplifier **140₁** provides signal amplification when input signal **102** and therefore RF signals **132₁** and **132₂** are small. Amplifier **140₂** remains turned off until RF signal **132₂** reaches a certain threshold level. Near this threshold level, amplifier **140₁** is close to saturation, and amplifier **140₂** turns on to supply the output-signal portion that tends to be clipped off by the near-saturation operating regime of amplifier **140₁**. This complementary action of amplifiers **140₁** and **140₂** enables transmitter **100** to advantageously have relatively high power efficiency for a wide range of input-signal levels. A more detailed explanation of how high power efficiency can be achieved for amplifiers **140₁** and **140₂** is provided below in reference to FIG. 3.

In addition to producing output signal **152** by properly combining signals **142₁** and **142₂**, RF-output circuit **150** is configured to generate feedback signals **148₁-148₃** based on signals **142₁**, **142₂**, and **152** and supply these feedback signals to FBR circuit **120**. In one embodiment, feedback signal **148₁** provided by RF-output circuit **150** to FBR circuit **120** is an attenuated copy of signal **142₁**; feedback signal **148₂** is an attenuated copy of signal **142₂**; and feedback signal **148₃** is an attenuated copy of signal **152**. In various alternative embodiments, RF-output circuit **150** can be configured to provide to FBR circuit **120** only two of feedback signals **148₁-148₃**.

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and/or generate each of feedback signals **148₁-148₃** based on a respective different linear combination of signals **142₁**, **142₂**, and **152**.

In one embodiment, FBR circuit **120** comprises three feedback receivers (not explicitly shown in FIG. 1), each configured to process a corresponding one of feedback signals **148₁-148₃**. The typical processing performed by a feedback receiver includes down-converting the corresponding feedback signal **148** to baseband and applying analog-to-digital conversion to the resulting analog baseband signal to generate a corresponding digital feedback signal **118**. Digital feedback signals **118₁-118₃** generated by FBR circuit **120** correspond to analog feedback signals **148₁-148₃**, respectively.

In general, the gain, efficiency, and AM-PM (amplitude-to-phase modulation) characteristics (e.g., the insertion-phase change as a function of signal amplitude) of a power amplifier, such as power amplifier **140₁** or **140₂**, are all functions of both the output power and the load impedance. In a typical prior-art DPD scheme, the individual stimuli (input signals) for the carrier and peak stages of a Doherty power amplifier are generated by means of a 3-dB power splitter configured to split the RF signal that is generated based on a *single* pre-distorted digital signal generated by the DPD circuit. This means that the stimuli applied to the carrier and peak stages have a *fixed* phase relationship with one another. However, as already indicated above, the carrier and peak stages of a Doherty power amplifier are configured to operate in different regimes, which causes their output signals to generally have a phase mismatch between them. Moreover, this phase mismatch varies over time owing to the variations in the output-power level. Disadvantageously, this prior-art DPD scheme is not capable of equalizing the phase mismatch and relies mostly on amplitude pre-distortion for the suppression of IMD products.

This and other pertinent problems in the prior art are addressed in transmitter **100** by configuring DPD circuit **110** to generate individually pre-distorted digital signals **112₁** and **112₂** for amplifiers **140₁** and **140₂**, respectively, based on multiple digital feedback signals, e.g., two or three of signals **118₁-118₃**. These feedback signals provide sufficient information to enable the DPD circuit to implement both amplitude pre-distortion and phase equalization for amplifiers **140₁** and **140₂**. In part due to a relatively small phase mismatch between output signals **142₁** and **142₂**,

transmitter **100** is able to better suppress IMD products in its output signal (i.e., signal **152**) than a comparable prior-art transmitter.

In one configuration, DPD circuit **110** uses digital feedback signals **118₁-118₃** to adaptively pre-distort input signal **102** to generate individually pre-distorted digital signals **112₁** and **112₂**. Pre-distorted digital signal **112₁** is applied to a transmitter **130₁**, where it is first converted into a corresponding analog signal (not explicitly shown in FIG. 1). Transmitter **130₁** then up-converts this analog signal from baseband to generate RF signal **132₁**. Pre-distorted digital signal **112₂** is similarly processed in a transmitter **130₂** to generate RF signal **132₂**. As already indicated above, RF signals **132₁** and **132₂** are the input signals (stimuli) that are applied to amplifiers **140₁** and **140₂**, respectively.

DPD circuit **110** is configured to generate pre-distorted digital signal **112₁** by applying a first nonlinear function to input signal **102**, wherein the first nonlinear function creates an expanding nonlinearity that is an approximate inverse of the compressing nonlinearity of (e.g., compressive amplitude distortion in) amplifier **140₁**. DPD circuit **110** is further configured to generate pre-distorted digital signal **112₂** by applying a second nonlinear function to input signal **102**, wherein the second nonlinear function creates a nonlinearity that is an approximate inverse of the nonlinearity of amplifier **140₂**. As already indicated above, the first and second nonlinear functions usually differ from one another due to different operating configurations of amplifiers **140₁** and **140₂**.

In various alternative configurations, DPD circuit **110** can similarly apply other types of first and/or second nonlinear functions to input signal **102** to generate pre-distorted digital signals **112₁** and **112₂**. In general, the first and second nonlinear functions are constructed in an inter-related manner to cause the forward signal path comprising DPD circuit **110**, transmitters **130₁** and **130₂**, amplifiers **140₁** and **140₂**, and RF-output circuit **150** to exhibit substantially linear signal-transfer characteristics. By substantially linear signal-transfer characteristics, it is meant that, with digital pre-distortion, the relationship between output signal **152** and input signal **102** can be approximated well by a constant gain, e.g., a complex or real gain value that does not depend on the input- (or output-) signal level within the intended dynamic range of transmitter **100**. Description of representative DPD circuits and algorithms that can

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be used to implement DPD circuit **110** can be found, e.g., in U.S. Patent Nos. 7,957,707, 7,904,033, 7,822,146, 7,782,979, 7,729,446, 7,606,324, 7,583,754, and 7,471,739, all of which are incorporated herein by reference in their entirety.

FIG. 2 shows a block diagram of a transceiver **200** that can be used in transmitter **100** (FIG. 1) according to one embodiment of the invention. Note that DPD circuit **110** shown in FIG. 2 is not part of transceiver **200**. Digital-to-analog converters (DACs) **234** and an I-Q modulator **236** can be used to implement transmitter **130₁** or transmitter **130₂**. Analog-to-digital converters (ADCs) **224** and an I-Q de-modulator **226** can be used to implement a portion of FBR circuit **120**. Transceiver **200** also has a local-oscillator (LO) source **244** that is configured to supply a local-oscillator (carrier-frequency) signal **246** to I-Q modulator **236** and I-Q de-modulator **226**. In a representative embodiment, transmitter **100** may have more than one instance of transceiver **200**.

In operation, I-Q de-modulator **226** demodulates feedback signal **148** in a conventional manner by mixing it with LO signal **246**. A resulting baseband signal **225** generated by I-Q de-modulator **226** has two components: an in-phase component **225_I** and a quadrature-phase component **225_Q**. Signals **225_I** and **225_Q** are analog signals that are converted into digital form by ADCs **224**. The resulting digital signals I_{fb} and Q_{fb} are components of the corresponding one of digital signals **118₁**-**118₃** (also see FIG. 1).

DPD circuit **110** uses digital signals I_{fb} and Q_{fb} to determine the amount of distortion in the forward signal path of transmitter **100** (FIG. 1). For example, a symbol received by DPD circuit **110** via digital signals I_{fb} and Q_{fb} can be combined with (e.g., summed with and/or subtracted from) one or more corresponding symbols received by the DPD circuit via the other one or more digital signals **118** (see FIG. 1). DPD circuit **110** then uses the corresponding original constellation symbol received via input signal **102** to determine the amount of pre-distortion that needs to be applied to the original I and Q components to counteract (e.g., cancel or significantly reduce) the distortion imposed by the forward signal path. The determined amount of pre-distortion can be partitioned, in any suitable manner, into a first portion and a second portion. The first portion, in form of the first nonlinear function, is applied to input signal **102** to generate pre-distorted digital signal **112₁**, while the second portion, in

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form of the second nonlinear function, is similarly applied to input signal **102** to generate pre-distorted digital signal **112₂**. Similar to signals **102** and **118**, signal **112** is shown as having two components: an in-phase component labeled I_{pd} and a quadrature-phase component labeled Q_{pd} . Note that FIG. 2 shows the generation of only one of pre-distorted digital signals **112₁** and **112₂**. The other one of these signals can be similarly generated.

Components I_{pd} and Q_{pd} of pre-distorted digital signal **112** are converted, in DACs **234**, into analog signals **235_I** and **235_Q**, respectively. I-Q modulator **236** then uses analog signals **235_I** and **235_Q** to modulate LO signal **246**. The resulting modulated carrier signal is RF signal **132** (also see FIG. 1). As already indicated above, signal **132** generated by I-Q modulator **236** can be one of signals **132₁** and **132₂** (see FIG. 1). The other one of these signals can be similarly generated.

FIG. 3 shows a circuit diagram of an RF circuit **300** that can be used as RF-output circuit **150** (FIG. 1) according to one embodiment of the invention. RF circuit **300** comprises a transcoupler **310**, an impedance transformer **320**, a directional coupler **330**, and six terminals labeled A through F. The impedances indicated in FIG. 3 are exemplary and correspond to an implementation in which each of the external terminals is intended for being connected to a 50-Ohm line, driver, load, or terminator. One of ordinary skill in the art will understand how to change the various impedance values shown in FIG. 3 to match RF circuit **300** to an impedance value different from 50 Ohm.

In a representative configuration, terminals A-F can be connected as follows. Terminal A is configured to carry feedback signal **148₁** (see FIGs. 1 and 2). Terminal B is configured to carry feedback signal **148₂** (see FIGs. 1 and 2). Terminal C is configured to receive amplified signal **142₁** (see FIG. 1). Terminal D is configured to receive amplified signal **142₂** (see FIG. 1). Terminal E is configured to carry feedback signal **148₃** (see FIGs. 1 and 2). Terminal F is configured to apply output signal **152** to load **160**.

This representative configuration can be modified to produce several alternative configurations. For example, three different alternative configurations can be obtained by changing the connection of terminal A, B, or E from the above-

indicated to a 50-Ohm terminator. In each of these three alternative configurations, RF circuit **300** will provide only two of feedback signals **148₁**-**148₃**.

Transcoupler **310** is a four-terminal device having two parallel branches **312** and **314** that are located sufficiently close to each other for an RF signal propagating through branch **314** to electromagnetically couple into branch **312**. Branch **314** comprises a quarter-wave impedance inverter disposed between terminals C and D. The signal coupling between branches **312** and **314** is relatively weak, e.g., about -30 dB, which ensures a minimal influence of branch **312** on the operation of the quarter-wave impedance inverter in branch **314**.

In operation, the quarter-wave impedance inverter of branch **314** can be used to implement active load modulation for carrier stage **140₁**, for example, as follows (also see FIG. 1).

At low input-signal levels, peak stage **140₂** is in the off state while carrier stage **140₁** acts as a controlled current source. Peak stage **140₂** (ideally) sees infinite impedance, and the impedance inverter of branch **314** causes carrier stage **140₁** to see a higher than 50-Ohm impedance load. The higher impedance load causes carrier stage **140₁** to reach near-saturation when its output current reaches only about one half of its nominal maximum value. When carrier stage **140₁** is close to saturation, it advantageously works with nearly maximum power efficiency.

As soon as the input-signal level becomes sufficiently high to turn on peak stage **140₂**, the peak stage begins to apply additional current to terminal D. Peak stage **140₂** now acts as a controlled current source, and carrier stage **140₁** acts as a controlled voltage source. The additional current applied by peak stage **140₂** to terminal D causes an increase in the output impedance seen by the quarter-wave impedance inverter of branch **314**. Since the input and output impedances of a quarter-wave impedance inverter are related to one another as duals, the increase in the output impedance causes a corresponding decrease in the input impedance. Note that the input impedance of the quarter-wave impedance inverter of branch **314** is the load that is seen by carrier stage **140₁**. As the load of carrier stage **140₁** decreases, the output current of the carrier stage increases, with the output voltage remaining close to the saturation level.

As the input-signal level increases further, the output impedance of the quarter-wave impedance inverter of branch **314** keeps increasing, and the effective load of carrier stage **140₁** keeps decreasing. In this manner, the impedance inverter of branch **314** enables peak stage **140₂** to modulate the load of carrier stage **140₁** during high input-signal levels. The load modulation, in turn, keeps carrier stage **140₁** operating in a regime that is characterized by advantageously high power efficiency.

Impedance transformer **320** comprises a length of transmission line that is one-quarter of a wavelength long and has an impedance of about 35 Ohm. (Note that, for a device that has a desired operating-frequency range, the quarter-wave length typically corresponds to the center frequency of that operating range.) Since impedance transformer **320** is terminated at 50 Ohm by directional coupler **330**, it presents at terminal D an input impedance of 25 Ohm. The latter impedance matches the output impedance of two 50-Ohm transmission lines connected in parallel to terminal D.

Directional coupler **330** comprises branches **332** and **334**. Branch **334** operates to present a fixed 50-Ohm termination to impedance transformer **320**. The signal coupling between branches **332** and **334** is relatively weak, e.g., about -30 dB. Terminal G is connected to a 50-Ohm terminator **340**. Terminal E outputs an attenuated copy of the RF signal presented at terminal H by impedance transformer **304**.

Feedback signals S_A , S_B , and S_E collected at terminals A, B, and E, respectively, of RF circuit **300** can be used to directly measure effective transfer functions T_1 and T_2 of stages **140₁** and **140₂**, for example, based on Eqs. (1)-(3):

$$T_1 = \frac{S_A}{ap_1} \quad (1)$$

$$T_2 = \frac{S_B}{ap_2} \quad (2)$$

$$T_1p_1 + T_2p_2 = \frac{S_E}{c} \quad (3)$$

where a is a constant that represents the signal-coupling strength between branches **312** and **314**; c is a constant that represents the signal-coupling strength between branches **332** and **334**; and p_1 and p_2 represent pre-distorted signals **112₁** and **112₂**, respectively. The measurement can be done on line or using an appropriate off-line

calibration procedure. In principle, any two of Eqs. (1)-(3) are sufficient for the determination of transfer functions T_1 and T_2 , provided that the coupling strengths are known. The use of all three equations enables the determination of the ratio (a/c) of the coupling strengths and, as such, can be used when only one of the two coupling strengths is known. After the individual transfer functions of stages **140₁** and **140₂** are determined, their reciprocals can be used in a relatively straightforward manner for amplitude pre-distortion and phase equalization.

FIG. 4 shows a circuit diagram of an RF circuit **400** that can be used as RF-output circuit **150** (FIG. 1) according to another embodiment of the invention. In terms of its intended function, RF circuit **400** is generally analogous to RF circuit **300** (FIG. 3). Therefore, the above-described connections of terminals A-F apply to RF circuit **400** as well as to RF circuit **300**. However, one difference between RF circuits **300** and **400** is that the latter employs a transcoupler **450** that performs the functions that are similar to the above-described functions of both impedance transformer **320** and directional coupler **330** (see FIG. 3).

The use of transcoupler **450** can provide one or more of the following benefits/advantages:

- (1) A transmitter (e.g., transmitter **100**, FIG. 1) employing RF circuit **400** can have a relatively high power efficiency, e.g., because transcoupler **450** has a lower insertion loss than a series consisting of impedance transformer **320** and directional coupler **330**;
- (2) RF circuit **400** can have a relatively small size because transcoupler **450** occupies a relatively small area on a printed circuit board (PCB); and
- (3) The relatively small size of transcoupler **450** and the improved power efficiency of the corresponding power amplifier can be leveraged to reduce per-unit fabrication and operating costs.

As evident from the description of transcouplers **310** and **450** in FIGs. 3 and 4, a transcoupler is a circuit element that has two branches that can be referred to as the main branch and the auxiliary branch, respectively. The main branch has a length of about one quarter of the carrier wavelength and is configured to operate as an impedance inverter that presents a first impedance at the first end of the branch, said first impedance being proportional to an inverse of a second impedance presented to

the branch at the second end of the branch. If the second impedance is a fixed impedance, then the first branch operates as a quarter-wave impedance transformer. Branches **314** and **454** are the main branches in transcouplers **310** and **450**, respectively. The auxiliary branch is electromagnetically coupled to the main branch and configured to operate as a signal coupler that receives an attenuated copy of a signal from the main branch. Branches **312** and **452** are the auxiliary branches in transcouplers **310** and **450**, respectively.

FIG. 5 shows a top view of a microstrip circuit **500** that can be used to implement RF circuit **400** (FIG. 4) according to one embodiment of the invention. Circuit **500** comprises a dielectric substrate **502** and two conducting layers attached to the opposite (e.g., top and bottom) sides of the dielectric substrate. Only the patterned top layer is visible in the view provided in FIG. 5. The various microstrip shapes of this patterned layer define the circuit elements of circuit **500**. The bottom layer (typically referred to as the “ground plane”) is not visible in the view provided in FIG. 5. In a representative embodiment, the ground plane is not patterned and comprises a continuous layer of metal, such as copper.

Circuit **500** has seven terminals labeled A through G. The terminals labeled by the same letter in FIGs. 4 and 5 are functionally similar. Therefore, the terminals of circuit **500** can be electrically connected to external circuits, e.g., as already described above in reference to FIGs. 3 and 4.

Microstrips **512** and **514** are used to implement a transcoupler **510** that is analogous to transcoupler **310** (see FIGs. 3 and 4). Microstrip **514** is one-quarter of a wavelength long. Microstrip **512** is electromagnetically coupled to microstrip **514** using two interdigitated combs. One of the combs is electrically connected to microstrip **512** and is illustratively shown in FIG. 5 as having two fingers **516**. The other comb is electrically connected to microstrip **514** and is illustratively shown in FIG. 5 as having four fingers **518**. Two mitred bends **508** are used to electrically connect microstrip **512** to terminals A and B.

Microstrips **552** and **554** are used to implement a transcoupler **550** that is analogous to transcoupler **450** (see FIG. 4). Microstrip **554** is one-quarter of a wavelength long. Microstrip **552** is electromagnetically coupled to microstrip **554** using two interdigitated combs. One of the combs is attached to a side of microstrip

552 and is illustratively shown in FIG. 5 as having two fingers **556**. The other comb is attached to a side of microstrip **554** and is illustratively shown in FIG. 5 as having four fingers **558**. A mitred bend **508** is used to electrically connect microstrip **552** to terminal E. Microstrips **516** and **562** are used to electrically connect the ends of microstrip **554** to terminals D and F, respectively.

Circuit **500** also has an optional shunted stub **560** that is connected to transcoupler **550** as indicated in FIG. 5. Stub **560** is implemented using a microstrip **566** and a shunt **564** that is located at the distal end of that microstrip. Microstrip **566** is one-quarter of a wavelength long. Shunt **564** comprises one or more electrically conducting vias in dielectric substrate **502** that electrically connect the distal end of microstrip **566** to the ground plane, thereby short-circuiting stub **560**. One function of stub **560** is to alter the effective impedance of transcoupler **550** compared to the impedance that the transcoupler would have without the stub. The altered impedance advantageously has an imaginary part that is substantially nulled and has a very weak frequency dependence within the pertinent spectral range around the nominal carrier frequency.

Note that each of microstrips **506**, **512**, **514**, **552**, and **562** has a first specified width, and each of microstrips **554** and **566** has a second specified width that is greater than the first. In a representative embodiment, the first and second widths are selected so that (i) each of the RF-transmission lines represented by microstrips **506**, **512**, **514**, **552**, and **562** has an impedance of 50 Ohm and (ii) each of the RF-transmission lines represented by microstrips **554** and **566** has an impedance of 35 Ohm. One skilled in the art will understand how to select other respective widths for these two sets of microstrips to obtain other impedance values.

FIG. 6 shows a circuit diagram of a two-stage/branch amplifier circuit **600** according to one embodiment of the invention. Circuit **600** can be used, e.g., to implement a Chireix amplification scheme. A circuit diagram of the corresponding transmitter can be obtained, e.g., by replacing amplifiers **140₁** and **140₂** and RF-output circuit **150** in transmitter **100** (FIG. 1) by circuit **600**. More specifically, signals/lines **632₁**, **632₂**, **648₁**, **648₂**, and **652** in circuit **600** correspond to signals/lines **132₁**, **132₂**, **148₁**, **148₂**, and **152**, respectively, in transmitter **100**.

The Chireix amplification scheme of circuit **600** employs power amplifiers **640₁** and **640₂** connected in parallel as indicated in FIG. 6. Output signals **642₁** and **642₂** generated by amplifiers **640₁** and **640₂**, respectively, are combined in an RF-output circuit **660** comprising output-matching circuits **644₁** and **644₂** and transcouplers **650₁** and **650₂**. Amplifiers **640₁** and **640₂** are configured to generate signals **642₁** and **642₂** to be each other's complex conjugates and to have a constant envelope. After RF-output circuit **660** combines phase-modulated signals **642₁** and **642₂**, output terminal D of that circuit has the corresponding amplitude-modulated signal **652**.

Similar to RF-output circuits **300** and **400** (FIGs. 3 and 4), RF-output circuit **660** uses load-impedance modulation to achieve relatively high power efficiency for the amplifier stages. Transcoupler **650₁** is configured to invert the load impedance, which is then transformed by output-matching circuit **644₁** and presented to amplifier **640₁**. Transcoupler **650₂** is similarly configured to invert the load impedance, which is then transformed by output-matching circuit **644₂** and presented to amplifier **640₂**.

To properly convert phase-modulated signals **642₁** and **642₂** into amplitude-modulated signal **652**, the deviation from the prescribed complex conjugate-phase relationship between the two amplifier branches in circuit **600** needs to be as small as possible. Circuit **600** helps to achieve this result by providing feedback signals **648₁** and **648₂** for use with an appropriate DPD circuit that can be similar to DPD circuit **110** of transmitter **100**. Transcoupler **650₁** is configured to generate feedback signal **648₁**. Transcoupler **650₂** is similarly configured to generate feedback signal **648₂**. Based on these feedback signals, the corresponding DPD circuit can pre-distort signals **632₁** and **632₂** to achieve relatively accurate phase conjugation at terminal D.

In general, transcoupling elements analogous to transcouplers **450**, **550**, and **650** can be used in any multistage or multi-branch power-amplifier circuit configured to combine RF-output signals from two or more branches of amplifying elements and use feedback-based digital pre-distortion to linearize the overall transfer characteristics of the power amplifier, e.g., to suppress IMD products in its output signal. The above-described Doherty and Chireix amplification schemes are just two representative examples of such multistage power-amplifier circuits. From the description provided herein, one of ordinary skill in the art will be able to use

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transcoupling elements instead of conventional RF-circuit elements in various other circuits. Possible benefits/advantages of such use are already indicated above in reference to FIG. 4.

As used in this specification, the term “radio frequency” (RF) refers a rate of oscillation in the range of about 3 kHz to 300 GHz. This frequency may be the frequency of an electromagnetic wave or an alternating current in a circuit. This term should be construed to be inclusive of the frequencies used in wireless communication systems.

While this invention has been described with reference to illustrative embodiments, this description is not intended to be construed in a limiting sense.

Although RF circuit **400** (FIG. 4) has been described as being implemented using a microstrip technology, it can also be implemented using any other suitable technology, e.g., a coaxial technology or a planar (such as stripline, slotline, or planar-waveguide) technology. Other RF circuits disclosed in this specification can similarly be implemented using these technologies.

As used in the claims, the term “strip” should be construed to cover any conducting strip, such as a microstrip or a stripline, in the patterned layer of the corresponding planar circuit or printed circuit board.

In one embodiment, transcoupler **550** (FIG. 5) can be used in conjunction with one or more circuit elements that differ from directional coupler **510**. For example, instead of being connected to microstrips **506** and **514**, microstrip **554** of transcoupler **550** can be connected at the left (as viewed in FIG. 5) end thereof to a microstrip that has a width different from the width of microstrip **554** and the width of microstrip **562**.

Various modifications of the described embodiments, as well as other embodiments of the invention, which are apparent to persons skilled in the art to which the invention pertains are deemed to lie within the principle and scope of the invention as expressed in the following claims.

The present invention may be implemented as circuit-based processes, including possible implementation on a single integrated circuit.

Unless explicitly stated otherwise, each numerical value and range should be interpreted as being approximate as if the word "about" or "approximately" preceded the value of the value or range.

The use of figure numbers and/or figure reference labels in the claims is intended to identify one or more possible embodiments of the claimed subject matter in order to facilitate the interpretation of the claims. Such use is not to be construed as necessarily limiting the scope of those claims to the embodiments shown in the corresponding figures.

Although the elements in the following method claims, if any, are recited in a particular sequence with corresponding labeling, unless the claim recitations otherwise imply a particular sequence for implementing some or all of those elements, those elements are not necessarily intended to be limited to being implemented in that particular sequence.

Reference herein to "one embodiment" or "an embodiment" means that a particular feature, structure, or characteristic described in connection with the embodiment can be included in at least one embodiment of the invention. The appearances of the phrase "in one embodiment" in various places in the specification are not necessarily all referring to the same embodiment, nor are separate or alternative embodiments necessarily mutually exclusive of other embodiments. The same applies to the term "implementation."

Throughout the detailed description, the drawings, which are not to scale, are illustrative only and are used in order to explain, rather than limit the invention. The use of terms such as height, length, width, top, bottom, is strictly to facilitate the description of the invention and is not intended to limit the invention to a specific orientation. For example, height does not imply only a vertical rise limitation, but is used to identify one of the three dimensions of a three dimensional structure as shown in the figures. Such "height" would be vertical where the microstrips are horizontal but would be horizontal where the microstrips are vertical, and so on.

Also for purposes of this description, the terms "couple," "coupling," "coupled," "connect," "connecting," or "connected" refer to any manner known in the art or later developed in which energy is allowed to be transferred between two or more elements, and the interposition of one or more additional elements is

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contemplated, although not required. Conversely, the terms "directly coupled," "directly connected," etc., imply the absence of such additional elements.

The present inventions may be embodied in other specific apparatus and/or methods. The described embodiments are to be considered in all respects as only illustrative and not restrictive. In particular, the scope of the invention is indicated by the appended claims rather than by the description and figures herein. All changes that come within the meaning and range of equivalency of the claims are to be embraced within their scope.

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CLAIMS

What is claimed is:

1. An apparatus, comprising:

a digital pre-distortion circuit configured to pre-distort a digital input signal to generate a first pre-distorted digital signal and a second pre-distorted digital signal different from the first pre-distorted signal;

a first amplifier branch configured to generate a first amplified signal based on the first pre-distorted digital signal;

a second amplifier branch configured to generate a second amplified signal based on the second pre-distorted digital signal; and

a radio-frequency (RF) circuit configured to combine the first and second amplified signals to generate a combined signal, wherein:

the RF circuit is further configured to generate first and second feedback signals based on at least two of the first amplified signal, the second amplified signal, and the combined signal; and

the digital pre-distortion circuit is configured to generate the first pre-distorted digital signal and the second pre-distorted digital signal based on said first and second feedback signals to counteract nonlinearity in the first and second amplifier branches.

2. The apparatus of claim 1, wherein:

the first amplifier branch comprises:

a first transmitter configured to convert the first pre-distorted digital signal into a first RF signal; and

a first power amplifier configured to amplify the first RF signal to generate the first amplified signal;

the second amplifier branch comprises:

a second transmitter configured to convert the second pre-distorted digital signal into a second RF signal;

a second power amplifier configured to amplify the second RF signal to generate the second amplified signal.

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3. The apparatus of claim 2, wherein the first power amplifier and the second power amplifier are configured to operate as a carrier stage and a peak stage, respectively, of a Doherty power amplifier.

4. The apparatus of claim 2, wherein the first power amplifier and the second power amplifier are configured to operate as respective phase-modulating stages of a Chireix power amplifier.

5. The apparatus of claim 1, wherein:
the RF circuit is further configured to generate a third feedback signal; and
each of the first, second, and third feedback signals is an attenuated copy of a respective one of the first amplified signal, the second amplified signal, and the combined signal.

6. The apparatus of claim 1, further comprising:
a feedback-receiver circuit configured to:
down-convert the first feedback signal to generate a first digital baseband signal;
down-convert the second feedback signal to generate a second digital baseband signal; and
apply said first and second digital baseband signals to the digital pre-distortion circuit, wherein the digital pre-distortion circuit is configured to generate the first pre-distorted digital signal and the second pre-distorted digital signal based on said first and second digital baseband signals; and
an antenna configured to emit an electromagnetic wave corresponding to the combined signal.

7. The apparatus of claim 1, wherein the digital pre-distortion circuit is configured to counteract said nonlinearity by counteracting:
compressive amplitude distortion in at least one of the first and second amplifier branches; and
a phase mismatch between the first and second amplifier branches.

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8. The apparatus of claim 1, wherein the RF circuit comprises a first directional coupler, said first directional coupler comprising:

a first branch connected between an output port of the first amplifier branch and an output port of the second amplifier branch; and

a second branch electromagnetically coupled to the first branch and having first and second terminals, wherein the first feedback signal appears on the first terminal.

9. The apparatus of claim 8, wherein the RF circuit further comprises a transcoupler, said transcoupler comprising:

a respective first branch connected in series with the first branch of the first directional coupler; and

a respective second branch electromagnetically coupled to said respective first branch and having third and fourth terminals, wherein the second feedback signal appears on the third terminal.

10. A signal-amplification method, comprising:

pre-distorting a digital input signal to generate a first pre-distorted digital signal and a second pre-distorted digital signal different from the first pre-distorted signal;

generating a first amplified signal based on the first pre-distorted digital signal in a first amplifier branch;

generating a second amplified signal based on the second pre-distorted digital signal in a second amplifier branch;

combining the first and second amplified signals in a radio-frequency (RF) circuit to generate a combined signal; and

generating first and second feedback signals based on at least two of the first amplified signal, the second amplified signal, and the combined signal, wherein the step of pre-distorting comprises generating the first pre-distorted digital signal and the second pre-distorted digital signal based on said first and second feedback signals to counteract nonlinearity in the first and second amplifier branches.