

Description

This invention relates to circuitry for generating signal values between known values as for example in expanding or compressing video images.

5 In video signal expansion and compression systems it is desired to perform a time scaling of discrete-time signals. However, in order to realize a general scaling of the discrete-time axis for the transformation $y(m) = x(\alpha \cdot m)$, a major problem arises; the input signal $x(\alpha \cdot m)$ is undefined for non-integral values of its index ($\alpha \cdot m$). Interpolation is the solution to this problem. When the output requires a sample of the input at a time index with an undefined input value, an interpolated value must be supplied. A large body of literature exists on the
10 topic of interpolation, but several points are worth noting: a) interpolation which uses a large number of input samples weighted with a $\sin(x)/x$ function provides accurate results but is costly to implement for consumer apparatus; b) sample-and-hold interpolation is the easiest to implement but has generally poor performance; c) linear interpolation is relatively easy to implement and provides superior performance to the sample-and-hold technique, but exhibits increasing attenuation with increasing signal frequency; and d) higher order interpolation provides superior performance to linear interpolation but exhibits nonlinearities.

15 T. J. Christopher in U.S. Patent No. 4,694,414 described a relatively non-complex interpolator which exhibits relatively accurate performance and which is realized with a parallel combination of a two-point linear interpolator and a phase compensation filter. The compensation filter has a transfer function $H(z)$ given by

$$H(z) = -1 + z^{-1} + z^{-2} - z^{-3} \quad (1)$$

20 where z is the conventional "z" transform variable and the exponents thereof correspond to the number of sample intervals. It should be noted that the weighting coefficients are either plus or minus one. The amplitude characteristic of the filter $A(\Phi)$ is given by

$$A(\Phi) = 2 \cos(\Phi/2) - 2 \cos(3\Phi/2) \quad (2)$$

where Φ represents frequency in radians per second.

25 The compensation filter is cascaded with a gain element programmed with estimated gain values corresponding to the possible positions at which the system is designed to produce interpolated values. These gain values are derived by calculating the response error at a particular signal frequency. Since these gain values are not a function of frequency the response of the Christopher system contains residual errors.

30 The present invention is directed to provision of a relatively simple interpolation circuit, which has a substantially accurate response characteristic for all signal frequencies up to the Nyquist sampling limit of the system.

The present invention is a signal interpolator in accordance with the appended claims including the parallel combination of a linear interpolator and a compensating filter. The compensating filter is a finite impulse response filter including tap weights, successive ones of which follow a modified $\sin(x)/x$ function.

Brief Description of the Drawings

FIGURE 1 is a waveform diagram illustrating a sinc sampling function.

40 FIGURE 2 is a graphical representation of a normalized sinc function which may be utilized in an embodiment of the invention.

FIGURE 3 is a block diagram of an interpolator system embodying the invention.

FIGURE 4 is a block diagram of a compensating filter which may be implemented for the filter 22 in FIGURE 3.

45 It is well known that ideal interpolation can be achieved by convolving an input signal with a function S which expresses the impulse response of an ideal low pass filter. For continuous signals the function S is defined

$$S(t) = \sin(2\pi\beta t)/2\pi\beta t \quad (3)$$

50 where β is equal to the Nyquist frequency and the function of equation (3) is defined as the sinc function. The function $S(t)$ is illustrated in FIGURE 1. The discrete time interpolated value corresponding to a particular time may be calculated from a discrete time or sampled signal using the convolutions of $S(t)$ and the sampled signal $g(Tn)$. That is, an interpolated sample value $g(t_0)$ for sample time t_0 may be calculated from the sum of products $g(Tn) \times S_n(t_0)$ where $S_n(t_0)$ corresponds to a discrete time version of the function S and is given by

$$S_n(t) = \sin(2\pi\beta(t - nT))/(2\pi\beta(t - nT)) \quad (4)$$

More particularly, the interpolated value $g(t_0)$ is given by

$$g(t_0) = \sum_{n=-\infty}^{\infty} \{g(Tn) \times S_n(t_0)\} \quad (5)$$

Note however that it is not practical to perform the computation for all of the assigned values.

In order to implement the function in realizable hardware the following constraints are used. 1) The number of interpolated values between two sample points is limited to N (e.g., N=64). 2) Only M samples preceding and M samples following the point for which an interpolated value is to be calculated are used in the calculation. In the embodiment shown M is equal to four, thus a total of eight samples are used for each calculation.

The sampling function $S_n(t)$ is divided into a linear part and a nonlinear part. More particularly the terms

$$S_0(t) = F_0(t) + (1 - t/T) \quad (6)$$

$$S_1(t) = F_1(t) + t/T \quad (7)$$

and $S_n(t) = F_n(t)$ for values of n except zero and one.

The functions $F_n(t)$ are further defined.

$$F_0(t) = F_1(t) = k_0 F(t) \quad (8)$$

$$F_{-1}(t) = F_2(t) = k_1 F(t) \quad (9)$$

$$F_{-2}(t) = F_3(t) = k_2 F(t) \quad (10)$$

$$F_{-3}(t) = F_4(t) = k_3 F(t) \quad (11)$$

and

$$k_0 = S_0(T/2) - 0.5 \quad (12)$$

$$k_1 = S_1(T/2) - 0.5 \quad (13)$$

and the remaining k_n are given by

$$k_n = S_n(T/2) \quad (14)$$

The function $F(t)$ is defined

$$F(t) = \{S_{-1}(t) + S_2(t)\} / \{2S_2(T/2)\} \quad (15)$$

where the argument t in equation 15 corresponds to the position in time between the input sample points for which an interpolated value is calculated and the terms S_{-1} and S_2 in equation 15 conform to the sinc function as defined in equation 4. For example, assume that the point for which an interpolated value is to be calculated is between successive samples S_a and S_b and is a distance $(R/N)T$ from the first occurring sample S_a . The value $(1-R/N)T$ is substituted for the argument t in equation 15 where $R/N(T)$ defines the fractional portion of the sample period T. The values of $F(t)$ for N equal to 64 are shown graphically in FIGURE 2.

Substituting equations 6-14 into equation 5 results in

$$g(t_0) = (1 - R/N)g(0) + R/N g(T) + \\ + k_0 g(0) + k_1 g(T) + k_2 g(2T) + k_3 g(3T) + k_4 g(4T) \quad (16)$$

The first two terms correspond to linear interpolation. The latter terms correspond to a finite impulse response filter function multiplied by the variable gain function $F(t)$. The values k_n represent weighting coefficients applied to respective samples $g(nT)$. Table I illustrates the respective values of k_n for an eight tap filter.

TABLE I

$k_{-3} = -2/(7\pi) =$	-0.0909
$k_{-2} = 2/(5\pi) =$	0.1273
$k_{-1} = -2/(3\pi) =$	-0.2122
$k_0 = 2/\pi - 0.5 =$	0.1366
$k_1 = 2/\pi - 0.5 =$	0.1366
$k_2 = -2/(3\pi) =$	-0.2122
$k_3 = 2/(5\pi) =$	0.1273
$k_4 = -2/(7\pi) =$	-0.0909

The interpolation system is shown in FIGURE 3. In this embodiment it is in the environment of a video signal raster mapper where for example compressed widescreen image information is reformatted for widescreen im-

age reproduction. It is assumed that each horizontal line of video information consists of a sequence of compressed left side panel information, slightly expanded center panel information, and compressed right side panel information. The interpolator in this instance expands the right and left sidepanel information and compresses the center panel information to provide non-compressed/expanded lines of horizontal information for utilization by a widescreen display apparatus.

In FIGURE 3 the compressed/expanded video information is applied to a data input terminal which is coupled to a data buffer 10. The data buffer 10 includes a demultiplexing switch 12, two one-horizontal line buffer memories 14 and 16 and a multiplexing switch 18. The data buffer is controlled by a control signal generator 38 to load incoming data in one buffer memory while at the same time providing data (representing a previously stored line of information) from the second buffer memory to the interpolator circuitry. The two buffer memories alternate between receiving and outputting data. The receiving memory is clocked at the rate of occurrence of incoming samples while the outputting memory is clocked at a rate determined by the interpolation function. The output clock rate may in fact be the same as the input rate but operated in start/stop fashion.

A similar data buffer 44 is coupled at the output of the interpolator to receive interpolated samples at one rate and to provide interpolated samples at an output terminal OUT at a constant rate.

The control of the entire system is provided by a counter 40 and a read only memory 42, which provide control signals to the clock control generator 38, the values $F(t)$ to the nonlinear portion of the interpolator and the values R/N to the linear portion of the interpolator. At the beginning of each horizontal line interval, the counter 40 is reset to a predetermined value (e.g., zero), by a horizontal synchronization signal HORIZ. Thereafter the counter 40 begins counting cycles of a clock signal ($4f_{sc}$) which is synchronous with the incoming data signal and has a frequency at least as high as the incoming data rate. Each count value provided by the counter corresponds to a known position on the horizontal line of video information. The count values provided by the counter 40 are coupled as address values to the ROM 42. The ROM is preprogrammed at its respective address locations to provide the appropriate control signals to the generator 38 and to provide the appropriate values corresponding to $F(t)$ and R/N .

The actual interpolator includes: a non-linear signal path consisting of a compensation filter 22 and a multiplier 34; a linear signal path including a compensating delay element 20 and a linear interpolator 24; and a summing circuit 36 for adding the signals processed in the two signal paths. Signal from the data buffer 10 is coupled to both the linear and non-linear signal paths. In the nonlinear signal path the signal is filtered in the compensating filter 22 which is a finite impulse response filter having symmetrical tap coefficients corresponding to the values k_n . Output signal from the filter 22 is coupled to the multiplier 34 wherein it is multiplied by the values $F(t)$. Scaled values from the multiplier 34, which conform to the non-linear portion of equation 16, are coupled to one input terminal of the summing circuit 36, the output of which is coupled to the data buffer 44.

In the linear signal path, the input signal is coupled to a delay element 20 which compensates for the difference in processing delays between the linear and non-linear signal paths. The output terminal of the delay element 20 is coupled to a one sample delay element 26 and the minuend input terminal of a subtracter 28. Delayed samples from the delay element 26 are coupled to the subtrahend input terminal of the subtracter 28. Output differences from the subtracter are coupled to a multiplier 30 wherein they are multiplied by the value R/N . Respective output samples from the multiplier 30 and the delay element 26 are coupled to first and second input terminals of an adder 32. If the current sample provided by the delay element 20 is $g(1)$ then the current sample provided by the delay element 26 is $g(0)$. The output signals provided by subtracter 28, multiplier 30 and adder 32 are $(g(1)-g(0))$; $R/N(g(1)-g(0))$; and $R/N(g(1)-g(0)) + g(0)$ respectively. The terms of the output signal from the adder 32 may be rearranged to $R/N(g(1) + g(0) (1-R/N))$ which conforms to the linear response portion of equation 16. These sums are coupled to a second input terminal of the summing circuit 36.

FIGURE 4 illustrates exemplary circuitry for realizing the compensating filter 22. Since pairs of samples are weighted with like coefficients, these pairs are first combined and then weighted to reduce hardware. The particular filter shown is an eight tap filter, however a filter of more or less taps may be used.

In FIGURE 4 input signal is applied to the cascade connection of seven one-sample delay elements 52-64. Input signal and delayed signal from delay element 64 are coupled to respective input terminals of an adder 76. Output sums from adder 76 are coupled to a multiplier 86 wherein they are multiplied by the coefficient k_4 to generate the sum of products $k_{4g}(4T) + k_{4g}(-3T)$ which is equal to $k_{4g}(4T) + k_{3g}(-3T)$. The sum of products provided by the multiplier 86 is coupled to an adder 90 which provides the filter output signal corresponding to the term in brackets in equation 16.

Delayed signals from delay elements 52 and 62 are coupled to respective input terminals of an adder 74, the output of which is applied to a multiplier 84. Sums of signals provided by adder 74 are multiplied by the coefficient k_3 in multiplier 84 to produce the sum of products $k_{3g}(3T) + k_{3g}(-2T)$ which is equal to $k_{3g}(3T) + k_{2g}(-2T)$. Output signals from multiplier 84 are coupled to the adder 90.

Delayed signals from delay elements 54 and 60 are similarly coupled to an adder 72 and multiplier 82 combination which provide the sums of products $k_{2,g}(2T) + k_{1,g}(T)$ to the adder 90. Similarly, delayed signals from delay elements 56 and 58 are applied to an adder 70, multiplier 80 combination which provide the sums of products $k_{1,g}(T) + k_{0,g}(0)$ to adder 90. Adder 90 sums the output signals provided by the multipliers 80-86 to produce the filter output signal.

It should readily be appreciated that the compensating delay element 20 in FIGURE 3 may be eliminated by obtaining the signal which is applied to the linear interpolator from the appropriate delay element of the filter illustrated in FIGURE 4 (e.g., signal from delay element 56).

In addition the coefficients, k_n , listed in Table I may be modified slightly to facilitate hardware realization of the multipliers by using the closet binary ratio to the coefficient. For example, k_1 , k_2 , k_3 and k_4 may be 9, 14, 8 and 6 sixty fourths respectively, or 17, 27, 17 and 12 one-twenty-eighths respectively. Similarly, the values of $F(t)$ may be adjusted to equal a binary ratio. As such the multiplier may be realized with shift-and-add circuitry.

While the invention has been described in the environment of video processing, it is to be understood that it is applicable to processing any sampled data signal.

Claims

1. A sampled data interpolator having an input terminal for receiving a sampled data input signal; a linear interpolator (24) coupled to said input terminal for providing linearly interpolated samples at an output terminal thereof; a filter coupled to said input terminal, for providing filtered samples corresponding to a compensating signal; means (36) coupled to output means of said filter and linear interpolator for additively combining said linearly interpolated samples and said filtered samples; characterized in that said filter is a finite impulse response filter, having weighting means (80 - 86), for scaling said compensating signal by a normalised sinc function to provide scaled samples at said filter output means.

2. A sampled data interpolator as set forth in claim 1 characterized in that said normalized sinc function corresponds to

$$\frac{\frac{\sin\{\frac{\pi}{T}(d+T)\}}{\frac{\pi}{T}(d+T)} + \frac{\sin\{\frac{\pi}{T}(d-2T)\}}{\frac{\pi}{T}(d-2T)}}{2 \frac{\sin\{\frac{\pi}{T}(d_n-2T)\}}{\frac{\pi}{T}(d_n-2T)}}$$

where d corresponds to the position of an interpolated sample between two input samples in terms of a fraction of a sample period T , and d_n corresponds to a normalizing position typically $T/2$.

3. A sampled data interpolator as set forth in claim 1 characterized in that said finite impulse response filter has a transfer function, H , given by

$$H = \sum_{n=-M+1}^M k_n g(nT)$$

where n is an index; T represents a sample period; $g(nT)$ correspond to input sample values; M is a number equal to one half the number of input samples used by the filter to form a filtered sample, and k_n are given by



Delayed signals from delay elements 54 and 60 are similarly coupled to an adder 72 and multiplier 82 combination which provide the sums of products $k_{2,0}(2T) + k_{1,0}(T)$ to the adder 90. Similarly, delayed signals from delay elements 56 and 58 are applied to an adder 70, multiplier 80 combination which provide the sums of products $k_{1,0}(T) + k_{0,0}(0)$ to adder 90. Adder 90 sums the output signals provided by the multipliers 80-86 to produce the filter output signal.

It should readily be appreciated that the compensating delay element 20 in FIGURE 3 may be eliminated by obtaining the signal which is applied to the linear interpolator from the appropriate delay element of the filter illustrated in FIGURE 4 (e.g., signal from delay element 56).

In addition the coefficients, k_n , listed in Table I may be modified slightly to facilitate hardware realization of the multipliers by using the closest binary ratio to the coefficient. For example, k_1 , k_2 , k_3 and k_4 may be 9, 14, 8 and 6 sixty fourths respectively, or 17, 27, 17 and 12 one-twenty-eighths respectively. Similarly, the values of $F(t)$ may be adjusted to equal a binary ratio. As such the multiplier may be realized with shift-and-add circuitry.

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2. A sampled data interpolator as set forth in claim 1 characterized in that said normalized sinc function corresponds to

$$\frac{\sin\left\{\frac{\pi}{T}(d+T)\right\}}{\frac{\pi}{T}(d+T)} + \frac{\sin\left\{\frac{\pi}{T}(d-2T)\right\}}{\frac{\pi}{T}(d-2T)}$$

$$\frac{2 \sin\left\{\frac{\pi}{T}(d_n - 2T)\right\}}{\frac{\pi}{T}(d_n - 2T)}$$

where d corresponds to the position of an interpolated sample between two input samples in terms of a fraction of a sample period T , and d_n corresponds to a normalizing position typically $T/2$.

3. A sampled data interpolator as set forth in claim 1 characterized in that said finite impulse response filter has a transfer function, H , given by

$$H = \sum_{n=-M+1}^M k_n g(nT)$$

where n is an index; T represents a sample period; $g(nT)$ correspond to input sample values; M is a number equal to one half the number of input samples used by the filter to form a filtered sample, and k_n are given by



$$k_n \approx \frac{\sin\left\{\frac{\pi}{T}\left(\frac{T}{2} - nT\right)\right\}}{\frac{\pi}{T}\left(\frac{T}{2} - nT\right)}$$

5 for all n except zero and one, and

$$k_n \approx \frac{\sin\left\{\frac{\pi}{T}\left(\frac{T}{2} - nT\right)\right\}}{\frac{\pi}{T}\left(\frac{T}{2} - nT\right)} - 0.5$$

10 for n equal to zero and one.

Patentansprüche

- 15 1. Abtastdaten-Interpolator mit einem Eingangs-Anschluß zum Erhalt eines Abtastdaten-Eingangssignals;
- mit einem Linear-Interpolator (24), der mit dem Eingangs-Anschluß gekoppelt ist, zum Bereitstellen linear interpolierter Abtastwerte an seinem Ausgangs-Anschluß;
 - mit einem Filter, das mit dem Eingangs-Anschluß gekoppelt ist, zum Bereitstellen von gefilterten Abtastwerten, die mit einem Kompensationssignal korrespondieren;
 - 20 - mit einem Mittel (36), das mit einem Ausgangsmittel des Filters und dem Linear-Interpolator gekoppelt ist, zum additiven Kombinieren der linear interpolierter Abtastwerte und der gefilterten Abtastwerte;
- dadurch gekennzeichnet,
- daß das Filter ein FIR-Filter (Finite Impuls Response Filter) ist, mit einem Gewichtungsmittel (80 - 86) zum Skalieren des Kompensationssignals mit einer normalisierten sinc-Funktion, um skalierte Abtastwerte an dem Filter-Ausgangsmittel bereitzustellen.

2. Abtastdaten-Interpolator nach Anspruch 1,
- dadurch gekennzeichnet, daß die normalisierte sinc-Funktion korrespondiert mit

$$\frac{\frac{\sin\{(d+T)\pi/T\}}{\{(d+T)\pi/T\}} + \frac{\sin\{(d-2T)\pi/T\}}{\{(d-2T)\pi/T\}}}{2 \frac{\sin\{(d_n-2T)\pi/T\}}{\{(d_n-2T)\pi/T\}}}$$

30 wobei d mit der Position eines interpolierten Abtastwertes zwischen zwei Eingangs-Abtastwerten in Form eines Bruchteils einer Abtast-Periode T und d_n mit einer normalisierten Position von typisch T/2 korrespondiert.

3. Abtastdaten-Interpolator nach Anspruch 1,
- dadurch gekennzeichnet, daß das FIR-Filter (Filter mit begrenzter Einstellzeit) eine Übertragungsfunktion H hat, die vorgegeben ist durch

$$H = \sum_{-M+1}^M k_n \cdot g(nT)$$

45 wobei n ein Index ist;

wobei T eine Abtast-Periode repräsentiert;

wobei $g(nT)$ mit Eingangs-Abtastwerten korrespondiert;

wobei M eine Zahl gleich der Hälfte der Anzahl der Eingangs-Abtastwerte ist, die von dem Filter verwendet werden, um einen gefilterten Abtastwert zu bilden;

50 und wobei k_n gegeben wird durch

$$k_n \approx \frac{\sin\{(T/2 - nT)\pi/T\}}{\{(T/2 - nT)\pi/T\}}$$

55 für alle n mit Ausnahme von Null und Eins und

$$k_n \approx \frac{\sin\{(T/2 - nT)\pi/T\}}{\{(T/2 - nT)\pi/T\}} - 0.5$$

für n gleich Null und Eins.



Revendications

1. Un interpolateur de données échantillonnées possédant une borne d'entrée pour la réception d'un signal d'entrée de données échantillonnées ;
 un interpolateur linéaire (24) couplé à ladite borne d'entrée afin de fournir des échantillons interpolés linéairement sur une borne de sortie dudit interpolateur ;
 un filtre couplé à ladite borne d'entrée afin de fournir des échantillons filtrés correspondant à un signal de compensation ;
 un moyen (36) couplé à la sortie dudit filtre et interpolateur linéaire afin de combiner additivement lesdits échantillons linéairement interpolés et lesdits échantillons filtrés ;
 caractérisé en ce que ledit filtre est un filtre à réponse impulsionnelle finie, doté d'un moyen de pondération (80 - 86) en vue de l'étalonnage dudit signal de compensation par une sinc fonction normalisée, destinée à fournir des échantillons étalonnés aux bornes de ladite sortie de filtre.
2. Un interpolateur de données échantillonnées conforme à la Revendication 1, caractérisé en ce que ladite sinc fonction normalisée se présente sous la forme :

$$\frac{\frac{\sin \left\{ \frac{\pi}{T} (d+T) \right\}}{\frac{\pi}{T} (d+T)} + \frac{\sin \left\{ \frac{\pi}{T} (d+2T) \right\}}{\frac{\pi}{T} (d+2T)}}{2 \sin \left\{ \frac{\pi}{T} (d_n - 2T) \right\}} \frac{\pi}{T} (d_n - 2T)$$

- où d correspond à la position d'un échantillon interpolé entre les deux échantillons d'entrée en termes d'une fraction de période d'échantillonnage T, d_n correspondant à une position de normalisation caractéristique de T/2.
3. Un interpolateur de données échantillonnées conforme à la Revendication 1 caractérisé en ce que la fonction de transfert H dudit filtre à réponse impulsionnelle finie se présente comme suit :

$$H = \sum_{-M+1}^M k_n g(nT)$$

où n est un indice ; T représente une période d'échantillonnage ; $g(nT)$ correspond à des valeurs d'échantillonnage d'entrée ; M est un nombre égal à la moitié du nombre d'échantillons d'entrée utilisés par le filtre pour former un échantillon filtré, k_n étant défini par les équations ci-après :

$$k_n \cong \frac{\sin \left\{ \frac{\pi}{T} \left(\frac{T}{2} - nT \right) \right\}}{\frac{\pi}{T} \left(\frac{T}{2} - nT \right)}$$

pour tous les n sauf zéro et un, et



$$k_n \cong \frac{\sin \left\{ \frac{\pi}{T} \left(\frac{T}{2} - nT \right) \right\}}{\frac{\pi}{T} \left(\frac{T}{2} - nT \right)} - 0,5$$

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si n égale zéro et un.

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