

Description

The invention relates to a signal-source arrangement comprising

- a group of signal sources for generating substantially identical unit signals
- correction means for reducing mutual deviations in the unit signals from the signal sources by calibrating the signal sources in conformity with a calibration pattern recurring with a specific period, resulting in unit signals comprising similar by shaped spurious signals recurring with said period,
- combination means for combining a number of unit signals of the available unit signals to form an output signal.

The invention also relates to a digital-to-analog converter comprising such a signal-source arrangement. In the appended claims and the description "signal source" is to be understood to mean both a voltage source and a current source, so that the corresponding signals should be regarded as voltages and currents respectively.

An arrangement of the type defined in the opening paragraph is known from "A Self Calibration Technique for Monolithic High-Resolution D/A Converters", Digest of Technical Papers, 1989 IEEE International Solid-State Circuits Conference (ISSCC '89), pp. 22-23, February 1989. This known arrangement comprises a group of substantially identical current sources. The current sources each supply a unit current formed by the source-drain current of a MOS transistor. The magnitude of the source-drain current is dictated by a control voltage between the gate and the source of the MOS transistor. Combination means enable the unit currents to be combined in order to form one or more output currents which are multiples of the unit current. This is the case, for example, in a digital-to-analog converter in which the output currents are derived from the unit currents in conformity with a binary-ascending series.

As a result of the spread in transistor parameters the unit currents supplied by the MOS transistors are never perfectly equal to each other. This imposes a limitation on the accuracy of a digital-to-analog converter comprising such current sources. In the known current-source arrangement the equality of the current sources is improved in that the current sources are recalibrated continually by correction means. By means of a control circuit the control voltage across a capacitor arranged between the gate and source of the MOS transistor is then controlled in such a way that the source-drain current is equal to a reference current. When all the current sources have been calibrated the cycle is repeated. By means of this calibration method it is possible to obtain a group of current sources which are identical to each other with a very high accuracy. However, a consequence of the meth-

od is that the control voltage between the gate and the source of the MOS transistors does not remain constant between two consecutive calibration cycles as a result of charge leakage of the capacitor between the gate and source electrodes of the MOS transistors. This gives rise to ripple on the control voltage, so that the unit currents may also exhibit ripple components. Moreover, other spurious signals may arise as a result of calibration. For example, the alternate turn-on and turn-off of each of the current sources by means of the control circuit is attended by switching transients on the gates of the MOS transistors, which gives rise to a spurious signal in the drain-source current. Therefore, calibration results in all the unit currents exhibiting a substantially similar spurious signal having a period corresponding to the duration of one calibration cycle.

When the unit currents are combined to form larger output currents the spurious signals cumulate. The accumulation of the spurious signals restricts the accuracy of the output currents, which in the case of a digital-to-analog converter results in a reduced accuracy and dynamic range.

It is an object of the invention to provide a signal-source arrangement comprising means to minimize the influence of the spurious signals.

According to the invention a signal-source arrangement of the type defined in the opening paragraph is therefore characterized in that at least one of the correction means and the combination means is adapted to select unit signals for the output signal in such a way that relative to the spurious signal of one of the selected unit signals the spurious signals of the selected unit signals exhibit time shifts whose average value as closely as possible approximates to half the period and whose absolute values differ from each other to a maximal extent.

On account of the calibration sequence and/or the combination sequence of the calibrated signal sources the resulting spurious signals in the output signals will have a minimal amplitude, or a repetition rate which is a multiple of the calibration frequency, or a combination of these two possibilities. Thus, an improved spurious signal suppression and hence more accurate output signals can be obtained by the same means. When filters are employed for the rejection of spurious signals in the output signals the filters can be simplified or may even be dispensed with.

The invention will now be described in more detail, by way of example, with reference to the accompanying drawings in which:

Fig. 1 shows the basic diagram of a current-source arrangement comprising calibrated current sources,

Fig. 2 is the circuit diagram of an embodiment of a current-source arrangement comprising calibrated current sources,

Fig. 3 shows a calibrated current source and the

associated spurious-signal waveforms,

Fig. 4 shows combined calibrated current sources and associated spurious-signal waveforms,

Fig. 5 shows calibrated current sources arranged in accordance with the invention and the associated spurious-signal waveforms,

Fig. 6 shows alternative spurious-signal waveforms of calibrated signal sources arranged in accordance with the invention,

Fig. 7 shows a calibrated voltage source,

Fig. 8 shows alternative spurious-signal waveforms of calibrated signal sources arranged in accordance with the invention, and

Fig. 9 shows a digital-to-analog converter comprising a current-source arrangement in accordance with the invention.

Fig. 1 shows a basic diagram of a current-source arrangement comprising calibrated current sources. The arrangement is constructed to supply N substantially identical unit currents at outputs 1 to N , to which loads, which are not shown for simplicity, can be connected. The arrangement comprises $N+1$ current sources 2.1 to 2. $N+1$, which comprise transistors T1 to T. $N+1$. The current sources further have control inputs 3.1 to 3. $N+1$ for controlling the drive voltage and hence the current in the transistors T.1 to T. $N+1$. The arrangement further comprises correction means 4 comprising a correction circuit 5, including a reference-current source 6, for supplying a control signal to one of the control inputs 3.1 to 3. $N+1$ and comprising a switching network 7 for coupling each time one of the current sources 2.1 to 2. $N+1$ to the correction circuit 5 and for coupling the other current sources to the outputs 1 N in conformity with a cyclic pattern.

In this arrangement in every period of a cycle N current sources supply the output currents to the outputs 1 to N , the remaining current source being coupled to the correction circuit 4. In this correction circuit the current from the relevant current source is compared with the reference current from the source 6 and a control signal applied to the control input 3 of the current source by the correction circuit 5 controls the drive voltage of the transistor 2 in such a way that the current from the current source becomes equal to the reference current. In the next period of the cycle the corrected current source 2 is replaced with an uncorrected current source 2 by means of the switching network 7. In this way the currents from all the current sources 2.1 to 2. $N+1$ are corrected successively and continually. As a result of this, the currents at the outputs 1 to N are accurately equalized to the reference current. Since a signal source to be corrected is disconnected from the actual current-source arrangement the correction circuit 5 will not disturb the operation of the current-source arrangement. The unit currents at the outputs 1 to N remain available continuously.

Fig. 2 shows an embodiment of a calibrated cur-

rent-source arrangement in greater detail. The arrangement comprises four current sources constituted by the transistors T1 to T4 with capacitors C1 to C4 arranged between the gate and source electrodes. By means of the switches S1.1 to S4.1, S1.2 to S4.2 and S1.3 to S3.3 each time three of the four transistors T1 to T4 can be coupled to the outputs 1, 2 and 3 and the remaining transistor is coupled to the inputs 10 and 11 of the correction circuit 5. Said switches are controlled in a cyclic pattern in the present example by means of a shift register 14 under control of a clock 15.

The Figure illustrates the situation in which the drain-source currents I1, I3 and I4 of the transistors T1, T3 and T4 are applied to the outputs 1, 2 and 3 while the drain-source current I2 of the transistor T2 is applied to the input 11 of the correction circuit 5. The switches S1.1, S3.1 and S4.1 are open while the switch S2.1 is closed, so that the gate electrode of the transistor T2 is coupled to the input 10. In the present example of correction circuit comprises a reference current source 6, which supplies a current Iref to the interconnected inputs 10 and 11.

As a result of this direct connection between the inputs 10 and 11 the drain of the transistor T2 is connected to its gate. The current source 6 now controls the voltage on the capacitor C2 in such a way that the current I2 is accurately equalized to the reference current Iref. In the next clock period the transistor T2 is connected to the output 2 by means of the switches S2.2 and S2.3 and the switch S2.1 is opened. The voltage on the capacitor C2 therefore remains available, so that the current I2 in the transistor T2 remains accurately equal to the current Iref. In the same clock period one of the other three transistors, for example the transistor T3, is connected to the inputs 10 and 11 of the correction circuit and the control voltage on the capacitor C3 is adapted in such a way that the current I3 becomes accurately equal to the current Iref. In this way the currents I1 to I4 from the transistors T1 to T4 are successively and continually equalized to the current Iref. As a result of this, currents which are accurately equal to each other will appear at the outputs 1, 2 and 3.

Fig. 3a shows a suitable example of one of the calibrated current sources in the arrangement shown in Fig. 2, like parts bearing the same reference numerals. The switch S2.1 is constructed as a transistor T5 whose gate 12 is controlled in a suitable manner by means of a switching signal Usw from the shift register 14. A current source 13 representing a leakage current IL is shown in parallel with the capacitor C2. The leakage current IL is caused *inter alia* by the reverse source-substrate diode of the transistor T2. The presence of the leakage current causes the gate-source voltage Vgs of T2 to decrease between two calibration cycles. This is illustrated in Fig. 3a, in which Tc is the period of the calibration cycle. This

gives rise to a ripple-voltage component on the gate-source voltage V_{gs} of the transistor T2 of the order of magnitude of a few mV, which is converted substantially linearly into a similar ripple in the drain-source current I_{ds} of the transistor T2.

The switching signal U_{sw} which connects and disconnects the current source T2 to be calibrated to/from the correction means can also affect the gate-source voltage V_{gs} and hence the drain-source current I_{ds} of the transistor T2 as a result of, for example, capacitive crosstalk. Fig. 3 by way of example shows a possible signal waveform, which may be a different group in practice. Fig. 3 shows that the unit currents I_{ds} from the individual calibrated current sources comprise a spurious signal caused by the calibration process itself and having a period equal to the period T_c of the calibration cycle. The signal waveform of the spurious signal may be a mixture of the waveforms given in Figs. 3b and 3c, but in practice the spurious signal may have a different waveform.

The calibrated current sources 2.1 to 2.N in the current-source arrangement shown in Fig. 1 can be used for various purposes. It is common practice to use the unit currents I from the individual current sources 2 2.N in order to combine them so as to obtain larger output currents. In a digital-to-analog converter this combination is effected in such a way that the output currents form a binary ascending series. When I is the unit current, the first output current is then I , the second output current is $2I$, the third is $4I$, the fourth is $8I$ etc. Fig. 4a shows a calibrated current-source arrangement for use in a 3-bit digital-to-analog converter, in which for simplicity all the circuit elements discussed so far are symbolized by eight current sources 21 to 28, all having an intensity I and being calibrated in the sequence 21, 22, ..., 28, yielding eight equal unit currents I_1 to I_8 . The unit currents I_1 , I_2 , I_3 and I_4 are combined in combination means 20, shown diagrammatically, to form an output current I_{1234} available at the terminal 29. The unit currents I_5 and I_6 are combined to form an output current I_{56} at terminal 30, the unit current I_7 being applied directly to the terminal 31. By means of switches, not shown, the currents I_{1234} , I_{56} and I_7 are summed under control of a digital input signal to form an analog output current.

Fig. 4b gives the spurious signals i_1 to i_8 resulting from the leakage current in the current sources 21 to 28. Fig. 4c shows resulting spurious signals i_{1234} and i_{56} in the output currents I_{1234} and I_{56} respectively. The amplitudes of the spurious signals have increased relative to those of the spurious signals i_1 to i_8 .

Figs. 5a, b and c show the same group of calibrated current sources 21 to 28 as in Fig. 4 and the associated spurious signals like parts bearing the same reference numerals. In the combination means 20 the currents I_1 , I_3 , I_5 and I_7 are now combined to form an

output current I_{1357} at terminal 29, and the currents I_2 and I_6 are combined to form an output current I_{26} at terminal 30, a current I_4 being obtained at terminal 31. Fig. 5b again shows the individual spurious signals i_1 to i_8 the resulting spurious signals i_{1357} and i_{26} in the respective output currents I_{1357} and I_{26} being shown in Fig. 5c. It is easy to see that the resulting spurious signals are minimized by the selected combination of current sources. The peak-to-peak value of the ripple in the currents I_{1357} and I_{26} in the combination shown in Fig. 5a is equal to that of the ripple in the individual currents I_1 to I_8 . This very favourable minimum value is obtained if the average value of the shifts in time of the spurious signals i relative to that of one of the combined currents is equal to half the period T_c and if, in addition, those currents I_i are combined whose spurious signals have a maximal shift in time relative to one another. In Fig. 5b the shifts in time of the spurious signals i_3 , i_5 and i_7 relative to i_1 are represented by D_{13} , D_{15} and D_{17} and have the values $2/8 T_c$, $4/8 T_c$ and $6/8 T_c$ respectively, so that their average value is $1/3 \cdot 12/8 T_c = 1/2 T_c$. The same applies to the time shift of i_6 relative to i_2 , which shift is represented by D_{26} and is equal to $4/8 T_c = 1/2 T_c$. The spurious signals i_1 , i_3 , i_5 and i_7 moreover have the maximal time shift $2/8 T_c$ relative to one another. In contrast, the favourable minimum value of the spurious signal is not obtained if the I_1 , I_3 , I_4 , I_5 are combined to form an output current I_{1345} . In this case the average time shift between the spurious signals i_3 , i_4 and i_5 relative to i_1 is equal to half the period $1/2 T_c$ but the spurious signals i_3 , i_4 and i_5 have a smaller shift in time relative to one another than the signals i_3 , i_5 and i_7 .

For the current-source arrangement shown in Fig. 4 and Fig. 5 it has been demonstrated that for a given calibration sequence such a combination pattern can be obtained in the combination means 20 such that the combined currents exhibit a minimal spurious component. Conversely, i.e. for a given combination pattern, it will be evident that a suitable calibration sequence can be obtained with the same result. In the current-source arrangement shown in Fig. 4 the current sources 21, 22, ..., 28 should then be calibrated in the sequence 21, 25, 22, 27, 23, 26, 24, 28. If the current-source arrangement is of the type shown in Fig. 2 the calibration sequence can be changed by accordingly applying the control signals from the shift register 14 to the switches of the current sources.

Figs. 6a, b, c and d by way of example show four other spurious signals i_1 to i_8 which can occur in the current-source arrangement shown in Figs. 5a and 6a. The difference between the spurious signal i_{1234} of the combined currents I_1 , I_2 , I_3 and I_4 and the spurious signal i_{1357} of the combined currents I_1 , I_3 , I_5 and I_7 is shown for each of the four examples. Fig. 6a shows spurious signals of the type as described with

reference to Fig. 3c. The amplitudes of the spurious signals i1234 and i1357 are equal but the repetition rate of the spurious signal i1357 is four times as high as that of i1234. When filters for the output currents are used in order to reject spurious signals a higher frequency is more favourable because this simplifies filtering of the resulting spurious signal or because by means of the same filter a far better suppression of the spurious signal is obtained, yielding a more accurate digital-to-analog converter. In certain cases the quadrupled frequency may even be situated far outside the frequency band of the signal to be processed so that no spurious-signal filters at all are needed. The example shown in Fig. 6b relates to a more complex spurious signal. The amplitudes of the spurious signals i1234 and i1357 are substantially equal but the frequency of the spurious signal i1357 is four times as high as in i1234. In the example given in Fig. 6c the amplitude of the spurious signal i1357 is constant and in the example given in Fig. 6d the spurious signal i1357 has not only a smaller amplitude but also a higher frequency than in i1234.

The examples of combinations of spurious signals relate to current sources. It will be evident that the same signal waveforms may also apply to voltage sources. Fig. 7 shows an arrangement comprising voltage sources. The arrangement shown in Fig. 7a is substantially identical to that in Fig. 3a and corresponding reference numerals have the same meanings. A resistor 14 is arranged in series with the source of the transistor T2. The voltage drop across this resistor 14 is proportional to the calibrated current I_{ds} and is available as a unit voltage U on the terminal 13, which is connected to the source of the transistor T2. Fig. 7b shows an adding circuit for combining the unit voltages U1, U2, U3, ... The terminals 13 of the calibrated voltage sources are connected to resistors 15 and to the inverting input of an amplifier 17 to which negative feedback is applied by means of a resistor 14 and which has its output connected to the output terminal 18.

The advantageous method of combining calibrated signals, voltages or currents or the advantageous choice of the calibration sequence of the combined signals in order to reduce the resulting spurious signal in the combined signals can be applied to any number of signal sources and any possible combination of signals from the signal sources.

Fig. 8 shows an example comprising five signal sources whose spurious signals i1 to i5 are shown in Fig. 8a. The five sources in Fig. 8b are combined in two ways in the ratio 2 : 2 : 1. In Fig. 8c this in the ratio 3 : 1 : 1. The average value of each of the time shifts D13 and D24 of the signals i13 and i24 in Fig. 8b is $2/5 T_c$ and is therefore the closest approximation to half the period $1/2 T_c$. The same applies to the time shifts D14 and D25 which have an average value of $3/5 T_c$, the average value of the time shifts D13 and

D15 in the signal i135 in Fig. 3c is $1/2 \cdot 6/5 = 3/5 T_c$ and is again an optimal approximation to half the period $1/2 T_c$. In all the combined signals in the examples shown in Figs. 8b and 8c the repetition rate is doubled.

The combination sequence or calibration sequence as described above is very suitable for use in a digital-to-analog (DA) converter. Fig. 9 shows an embodiment of a DA converter comprising current-source arrangements in accordance with the invention. The present example is an 8-bit DA converter. It comprises a current-source arrangement 50, shown diagrammatically, including 18 current sources whose currents are substantially equalized in the above manner to the reference current I_{ref} from a current source 52 in a correction circuit 51. One current I_{ref} of the 18 output currents is used as the reference current for the correction circuit 61 of a second current-source arrangement 60 comprising sixteen current sources, whose currents are made equal to the current I_{ref} in the manner described above. Fifteen of the sixteen currents in the arrangement are combined in such a way that a binary-weighted series of currents $I_{ref}, 2I_{ref} \dots 8I_{ref}$ is obtained. The sixteen other currents from the current-source arrangement 50 are combined to form a current $16I_{ref}$, which is applied as the reference current to the correction circuit 71 of a third current-source arrangement 70 comprising sixteen current sources, whose currents are made equal to the current $16I_{ref}$ in the manner as described above. Again fifteen of the sixteen currents of the current-source arrangement 70 are combined in such a way that a binary-weighted series $16I_{ref}, 32I_{ref} \dots 128I_{ref}$ is obtained. The output currents of the current-source arrangements 60 and 70 are used in known manner to convert a digital input code into an analog output signal.

In both cases the output currents from the sixteen available current sources I1 to I16 are derived from the currents I1, I3, I5, I7, I9, I11, I13, I15 for the output currents $128I_{ref}$ and $8I_{ref}$; from the currents I4, I8, I12 and I16 for $64I_{ref}$ and $4I_{ref}$; from the currents I2 and I10 for $32I_{ref}$ and $2I_{ref}$, and from the current I6 or the current I14 for $16I_{ref}$ and I_{ref} . This is effected in a manner similar to that demonstrated for the arrangement shown in Fig. 5a.

The invention is not limited to the embodiments disclosed herein. The correction circuit for the calibration of the signal sources may also be constructed in a manner other than shown in Fig. 2, various modifications of the current source shown in Fig. 3a and the voltage source shown in Fig. 7a being possible.

Claims

1. A signal-source arrangement comprising
 - a group of signal sources (21...28) for gen-

reference to Fig. 3c. The amplitudes of the spurious signals I1234 and I1357 are equal but the repetition rate of the spurious signal I1357 is four times as high as that of I1234. When filters for the output currents are used in order to reject spurious signals a higher frequency is more favourable because this simplifies filtering of the resulting spurious signal or because by means of the same filter a far better suppression of the spurious signal is obtained, yielding a more accurate digital-to-analog converter. In certain cases the quadrupled frequency may even be situated far outside the frequency band of the signal to be processed so that no spurious-signal filters at all are needed. The example shown in Fig. 6b relates to a more complex spurious signal. The amplitudes of the spurious signals I1234 and I1357 are substantially equal but the frequency of the spurious signal I1357 is four times as high as in I1234. In the example given in Fig. 6c the amplitude of the spurious signal I1357 is constant and in the example given in Fig. 6d the spurious signal I1357 has not only a smaller amplitude but also a higher frequency than in I1234.

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The advantageous method of combining calibrated signals, voltages or currents or the advantageous choice of the calibration sequence of the combined signals in order to reduce the resulting spurious signal in the combined signals can be applied to any number of signal sources and any possible combination of signals from the signal sources.

Fig. 8 shows an example comprising five signal sources whose spurious signals I1 to I5 are shown in Fig. 8a. The five sources in Fig. 8b are combined in two ways in the ratio 2 : 2 : 1. In Fig. 8c this in the ratio 3 : 1 : 1. The average value of each of the time shifts D13 and D24 of the signals I13 and I24 in Fig. 8b is $2/5 T_c$ and is therefore the closest approximation to half the period $1/2 T_c$. The same applies to the time shifts D14 and D25 which have an average value of $3/5 T_c$, the average value of the time shifts D13 and

D15 in the signal I135 in Fig. 3c is $1/2 \cdot 6/5 = 3/5 T_c$ and is again an optimal approximation to half the period $1/2 T_c$. In all the combined signals in the examples shown in Figs. 8b and 8c the repetition rate is doubled.

The combination sequence or calibration sequence as described above is very suitable for use in a digital-to-analog (DA) converter. Fig. 9 shows an embodiment of a DA converter comprising current-source arrangements in accordance with the invention. The present example is an 8-bit DA converter. It comprises a current-source arrangement 50, shown diagrammatically, including 18 current sources whose currents are substantially equalized in the above manner to the reference current I_{ref} from a current source 52 in a correction circuit 51. One current I_{ref} of the 18 output currents is used as the reference current for the correction circuit 61 of a second current-source arrangement 60 comprising sixteen current sources, whose currents are made equal to the current I_{ref} in the manner described above. Fifteen of the sixteen currents in the arrangement are combined in such a way that a binary-weighted series of currents $I_{ref}, 2I_{ref}, \dots, 8I_{ref}$ is obtained. The sixteen other currents from the current-source arrangement 50 are combined to form a current $16I_{ref}$, which is applied as the reference current to the correction circuit 71 of a third current-source arrangement 70 comprising sixteen current sources, whose currents are made equal to the current $16I_{ref}$ in the manner as described above. Again fifteen of the sixteen currents of the current-source arrangement 70 are combined in such a way that a binary-weighted series $16I_{ref}, 32I_{ref}, \dots, 128I_{ref}$ is obtained. The output currents of the current-source arrangements 60 and 70 are used in known manner to convert a digital input code into an analog output signal.

In both cases the output currents from the sixteen available current sources I1 to I16 are derived from the currents I1, I3, I5, I7, I9, I11, I13, I15 for the output currents $128I_{ref}$ and $8I_{ref}$; from the currents I4, I8, I12 and I16 for $64I_{ref}$ and $4I_{ref}$; from the currents I2 and I10 for $32I_{ref}$ and $2I_{ref}$, and from the current I6 or the current I14 for $16I_{ref}$ and I_{ref} . This is effected in a manner similar to that demonstrated for the arrangement shown in Fig. 5a.

The invention is not limited to the embodiments disclosed herein. The correction circuit for the calibration of the signal sources may also be constructed in a manner other than shown in Fig. 2, various modifications of the current source shown in Fig. 3a and the voltage source shown in Fig. 7a being possible.

Claims

1. A signal-source arrangement comprising
 - a group of signal sources (21...28) for gen-



erating substantially identical unit signals (11..18),

- correction means (4) for reducing mutual level deviations in the unit signals from the signal sources by calibrating the signal sources in conformity with a calibration pattern recurring with a specific period (T_c), resulting in unit signals comprising similarly shaped spurious signals (11..18) recurring with said period,
- combination means (20) for combining a number of unit signals of the available unit signals to form an output signal,

characterized in that at least one of the correction means and the combination means is adapted to select unit signals for the output signal in such a way that relative to the spurious signal of one of the selected unit signals the spurious signals of the selected unit signals exhibit time shifts whose average value as closely as possible approximates to half the period and whose absolute values differ from each other to a maximal extent (Fig. 5C).

2. A digital-to-analog converter, characterized in that it comprises a signal-source arrangement as claimed in Claim 1.

Patentansprüche

1. Signalquellenanordnung mit:

- einer Gruppe von Signalquellen (21 ... 28) zur Erzeugung von im wesentlichen identischen Einheitssignalen (11 ... 18),
- Korrekturmitteln (4) zur Reduzierung von Pegelabweichungen zwischen den Einheitssignalen aus den Signalquellen durch Kalibrierung der Signalquellen in Übereinstimmung mit einem mit einer bestimmten Periode (T_c) wiederkehrenden Kalibrierungsmuster, was zu Einheitssignalen mit gleichförmigen Störsignalen (11 ... 18) führt, die mit genannter Periode wiederkehren,
- Kombinationsmitteln (20) zur Kombination einer Anzahl von Einheitssignalen aus den verfügbaren Einheitssignalen, um ein Ausgangssignal zu bilden,

dadurch gekennzeichnet, daß wenigstens eines der Korrekturmittel und der Kombinationsmittel eingerichtet ist, um Einheitssignale für das Ausgangssignal so zu selektieren, daß die Störsignale der selektierten Einheitssignale relativ zu dem Störsignal eines der selektierten Einheitssignale Zeitverschiebungen aufweisen, deren Durchschnittswert sich so dicht wie möglich der halben Periodendauer annähert und deren Absolutwerte sich voneinander in einem maximalen Ausmaß

unterscheiden (Figur 5c).

2. Digital-Analog-Umsetzer, dadurch gekennzeichnet, daß er eine Signalquellenanordnung nach Anspruch 1 umfaßt.

Revendications

1. Circuit de source de courant comportant

- un groupe de sources de signal (21,...28) pour engendrer des signaux unitaires sensiblement identiques (11,...18),
- des moyens de correction (4) pour réduire des écarts de niveau mutuels des signaux unitaires des sources de signal par calibration des sources de signal suivant une configuration de calibration se répétant à une période déterminée (T_c), de façon à donner naissance à des signaux unitaires comportant des signaux perturbateurs de forme similaire (11,...18) se répétant à la même période,
- des moyens combinateurs (20) pour combiner plusieurs signaux unitaires des signaux unitaires disponibles de façon à former un signal de sortie,

caractérisé en ce qu'au moins l'un des moyens de correction et des moyens correcteurs est agencé pour choisir des signaux unitaires pour le signal de sortie de façon que, par rapport au signal perturbateur de l'un des signaux unitaires choisis, les signaux perturbateurs des signaux unitaires choisis présentent des écarts dans le temps dont la valeur moyenne s'approche le plus étroitement possible de la moitié de la période et dont les valeurs absolues diffèrent autant que possible les unes des autres (figure 5c).

2. Convertisseur numérique-analogique, caractérisé en ce qu'il comporte un circuit de source de courant selon la revendication 1.

