

BACKGROUND OF THE INVENTION1. Field of the Invention

The present invention relates to the field of digital
5 communications.

2. Prior Art -

In a digital communications system, the function of the demodulator is to extract the digital information from a
10 modulated analog waveform. In the past, the demodulation function has been accomplished using analog signal processing techniques (mixers, filters, phase-locked-loops, etc.). With the advent of high-speed digital technology, it now possible to perform much of the demodulation function using discrete-
15 time or digital signal processing (DSP) techniques. Where an analog demodulator must be custom-tailored to the specific characteristics of a particular signal to be demodulated, a digital demodulator allows great flexibility in reprogramming to meet the requirements of a variety of systems having
20 different modulation types, channel characteristics, data rates, etc.

In a digital demodulation system, the process typically begins by sampling the analog waveform at a rate F_s .

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samples/sec and digitizing its amplitude using an A/D
(analog-to-digital) converter. Then the digitized samples
are processed through various mathematical operations to
extract the required information bits. The processing
5 operations usually include some type of filtering to
compensate for the effects of channel conditions or
modulation technique, as well as for the artifacts introduced
by the sampling process itself. It is usually necessary to
recover the timing (symbol rate) of the information bits from
10 the received signal because the precise timing is not known
at the receiver. This means that the symbol rate may not
necessarily be related to the sampling rate. Furthermore,
the symbol rate may not be constant over time; it may vary
somewhat due to imperfections in the timebases at the
15 transmitter and receiver or relative motion between the
transmitter and receiver.

According to the Nyquist criterion, the sampling rate
must be at least twice the highest frequency content of the
desired signal. In a digital system, the sampling rate must
20 be at least equal to the symbol rate, or greater, for better
performance. Typically, in current practice, a sampling rate
is chosen which is an integer multiple N of the symbol rate,
so that it is easy to reduce or decimate the sampling rate by
retaining only every N th sample and throwing out all others.
25 If a range of symbol rates is desired, then there must be
circuitry to generate a range of corresponding sampling
clocks. Since the exact timing of the received symbols is



generally not known, the sampling clock circuitry must also be capable of slewing in time to adjust the sampling instant to the optimal point.

The decimation process also requires a filter that
5 selects the desired signal components. The filtering can always be done before the decimation but this requires a very large computation to be performed at the higher sampling rate. There are well-known methods in which the decimation-by-N operation can be done before the filter (predecimation)
10 so that a smaller computation involving only every Nth sample can be performed at the lower decimated rate. In order to achieve the greatest computational efficiency, certain restrictions must be followed, mainly that such a filter can be designed to work only for one particular decimation ratio,
15 and there is no provision for adjusting the sampling instant.

Floyd M. Gardner, "Interpolation in Digital Modems--Part I: Fundamentals" (Floyd M. Gardner, IEEE Transactions on Communications, Vol. 41, No. 3, March 1993) describes an embellishment to the predecimation method, in which a
20 numerically-controller oscillator (NCO) is used to select which samples to process and to generate or look up the appropriate coefficients. This modification to the basic method allows for non-integral decimation ratios and for the slewing in time of the apparent sampling instant, while
25 preserving the computational efficiency of predecimation. But since the samples are predecimated, the filter must be



designed for the particular decimation ratio. If a selection of different ratios is desired, a different set of coefficients must be provided for each ratio. The number of taps, or length, of the filter may need to change too, to

5 maintain performance requirements over the range of decimation ratios.

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BRIEF SUMMARY OF THE INVENTION

The present invention addresses the combined operations of filtering and timing recovery in a digital demodulator.

In particular, this invention addresses the following

5 operations:

1. matched-filtering for equalization or wave-shaping;
2. $(\sin x)/x$ filtering for interpolation/decimation;
3. resampling to convert from input sampling rate F_s
to a lower, not necessarily commensurate, output
10 rate F_o ;
4. symbol time synchronization.

The Variable Rate Down-Sampling Filter of the present invention allows a continuous range of sample rates to be derived from input samples at a fixed rate. The output rate
15 does not have to be related to the fixed input rate in any integral or rational way, and in fact, the output rate can vary in time such as will occur when tracking a signal received from a station using a different timebase. A fixed sampling rate at the A/D Converter greatly simplifies the
20 design of the analog front end. A single anti-aliasing filter can be designed and precisely matched to the fixed sampling rate. Used with a frequency-modulated numerically controlled oscillator (NCO), the Down-Sampling Filter keeps the entire frequency-synthesis and time-tracking loop in the
25 digital domain. The need for an analog time-tracking loop to



adjust the sampling instant at the A/D converter is eliminated. The need for an analog frequency synthesizer to generate a variable sampling rate is also eliminated. System design and performance analysis are simplified as well by
5 eliminating the complication of hybrid analog-digital control loops.

With respect to the decimation process, there are well-known methods involving predecimation of the samples before filtering, which have the effect of reducing the amount of
10 computation necessary to produce decimated samples of a particular quality. But these methods restrict the decimation ratio to a fixed value because the filter characteristic must be designed for this ratio. The present invention does not predecimate, so it is not restricted to a
15 fixed ratio, but because of this, it is less efficient in terms of computational effort than the predecimation methods. However, the preferred embodiment of the present invention distributes the extra computational burden in a parallel-processing architecture suitable for a compact and efficient
20 implementation in VLSI in such a way that the physical complexity of the circuit is not much different than that of a circuit employing the predecimation method.



BRIEF DESCRIPTION OF THE DRAWINGS

Figures 1a, 1b, 1c and 1d are block diagrams of the Variable-Rate Down-Sampling Filter of the present invention, Figure 1a applying to a single channel system, Figure 1b
5 applying to a two channel system such as a quadrature modulated system wherein the two channels have the same characteristics, Figure 1c applying to a two channel system wherein channels A and B have the different characteristics, and Figure 1d applying to a system wherein multiple
10 coefficient generator-multiplier/accumulator units may be cascaded.

Figure 2 is a block diagram of the Numerically Controlled Oscillator (NCO) used in the Variable-Rate Down-Sampling Filter of Figure 1.

15 Figure 3 is a block diagram of the Coefficient Generator used in the Variable-Rate Down-Sampling Filter of Figure 1.

Figure 4 is a block diagram of the Multiplier-Accumulator Elements used in the Variable-Rate Down-Sampling Filter of Figure 1.

20 Figure 5 is a block diagram of the Variable-Rate Down-Sampling Filter of Figure 1 used in a Timing Recovery Loop.

Figure 6 is a graphical representation of the typical Filter impulse response.



Figure 7 is a block diagram for the Variable-Rate Down-Sampling Filter of the present invention in a Polyphase Structure.

5 Figure 8 is a block diagram for the Variable-Rate Down-Sampling Filter of the present invention in a Polyphase Structure showing greater detail than Figure 7.

Figure 9 is a block diagram for the Variable-Rate Down-Sampling Filter of the present invention in a Polyphase Structure with vertical sums.

10 Figure 10 is a block diagram for the Variable-Rate Down-Sampling Filter of the present invention in the preferred form of a Collapsed Polyphase Structure.

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DETAILED DESCRIPTION OF THE INVENTION

First referring to Figure 1a, the Variable-Rate Down-Sampling Filter of the present invention contains four major components: a Numerically-Controlled Oscillator (NCO), a Coefficient Generator, a cascade of Multiplier-Accumulator (MAC) elements, and an output Scaler. In a quadrature-modulated system where there are two channels (I and Q) of samples, a separate MAC array is required for each channel. But if the symbol rate and filtering requirements are the same on both channels, they can share the same coefficient generator, as shown in Figure 1b. Even if the multiple channels have different characteristics, a common NCO can be used to drive multiple coefficient generators and multiplier-accumulator chains, as shown in Figure 1c. While the two channels shown use the same value of M and the same width of address P to the coefficient generator, either or both P and M may be different for the two channels, though with the same sample rate, the same considerations would normally yield the same values of M and P for the two channels. Also the two coefficient generators, because they are addressed with the same address, may be a single RAM or ROM, in the example shown in Figure 1c being $2 * M * 2^P$ bits wide to output the two sets of coefficients simultaneously.

If the coefficient generator-multiplier/accumulator units are implemented as a unit, for example, as a VLSI circuit, multiple such units can be cascaded serially to increase the overall length of the filter, as shown in Figure 1d. In this case, the output of each unit feeds the initial value of the next, and all units share



the same input samples and the same phase and rollover signals from the numerically controlled oscillator. This embodiment would normally be used with RAM based coefficient generators, as the appropriate coefficients will depend on whether a particular MAC array and coefficient generator is being used alone or cascaded to another MAC array and coefficient generator. Note that such cascading may be under program control in a processor based system, so as to make the system reconfigurable under program control.

10 The Numerically Controlled Oscillator (Figure 2)

The Numerically Controlled Oscillator (NCO) generates timing and phase information for the Filter. As shown in Figure 2, the NCO is a large accumulator, consisting of an adder followed by a Register. The contents of the Register are fed back to one input of the adder. The other input of the adder is the value (Frequency Word) to be accumulated. The Register is clocked by the Sample Clock. At every clock tick, the value in the accumulator Register is incremented by the value presented at the input. When the accumulator increments past the top of its range, it "rolls over" and returns to the bottom. Thus the value of the accumulator Register traces out a periodic ramp or "sawtooth" function. The value of this Register at any given time relative to its full range represents the "phase" of the periodic function, and the interval between rollovers is one cycle or period of the function. The rate at which the ramp increases, and



therefore the frequency at which it rolls over, is determined by the increment value presented at the input to the accumulator. The increment value, called the Frequency Word, can be constant, or it can be varied in response to some
5 external control. In the former case, the NCO generates a fixed frequency. In the latter, the NCO is frequency-modulated and behaves very much like the Voltage-Controlled Oscillator (VCO) commonly found in analog frequency-synthesis circuits.

10 The Rollover frequency that the NCO generates is given by the relation:

$$F_o = (\text{Frequency_Word}/2^W) * F_s$$

where: F_o = the generated (Rollover) frequency

Frequency_Word = the binary value of the
15 increment input

W = the width, in bits, of the NCO accumulator
(Register and adder)

F_s = the frequency of the sampling clock

The precision of the NCO, that is, how exactly it can
20 represent a desired frequency, depends on the size of the accumulator. With an accumulator W bits wide, the NCO can represent any frequency with the precision of one part in 2^W of the reference frequency F_s . The interval between rollovers is not necessarily constant, but the average
25 interval $T_{avg} = F_s/F_o$ over a long time is a reasonably accurate representation of the desired frequency F_o .



While the frequency and period ($1/\text{frequency}$) of a periodic waveform are generally considered to be continuous quantities, the period that the NCO generates is discretized. The interval between rollovers is naturally an integral
5 number of cycles of F_s , the sample clock. However, if F_0 is not an exact divisor of F_s , the interval will not be constant; it will jitter between T and $T+1$ cycles of F_s , where T is the integer part of F_s/F_0 . But in the long term, the distribution of periods of length T and periods of length
10 $T+1$ will be such that the average period approximates the true value of F_s/F_0 , and therefore the frequency that the NCO generates approaches the true frequency F_0 .

The Coefficient Generator (Figure 3)

As may be seen in Figure 3, the coefficients for the
15 Filter are stored in a lookup table. The lookup table may be either fixed (ROM-based), or programmable (RAM-based) as shown in the Figure. The width of the table M is determined by the number of MAC elements in the Filter and the required precision (width in bits) of the coefficients; the depth is
20 determined by the required resolution in time. At every tick of the sampling clock, the NCO generates a new phase value. At each tick, the coefficients for all the elements are looked up simultaneously using the NCO phase as the index into the lookup table. In a two channel system such as in
25 Figure 1b, wherein the channel characteristics are the same,



only the data (samples) are different, the same coefficients are used for the two channels, as shown in Figure 1b.

The NCO phase accumulator (the Register of Figure 2) is generally quite large (32 bits is typical) in order to
5 provide a reasonably accurate representation of any frequency, but the Variable-Rate Down-Sampling Filter does not require this much precision for acceptable performance. The time resolution required is determined by the performance requirements of the system in which the present invention is
10 used, but is generally far less than the full precision of the NCO. Therefore, the NCO phase word (Phase output of Figure 2) can be truncated and only a few most-significant-bits (P bits, where $P \ll W$) are needed to index the coefficient lookup table.

15 The Multiplier-Accumulator (MAC) Chain (Figure 4)

The heart of the filter is the chain of M Multiplier-Accumulator (MAC) elements shown in Figure 4. The number of elements M in the chain is to be determined by system requirements for the characteristics of the filter function.
20 Each element has a multiplier, an accumulator, and an input selector or mux SEL. At every tick of the sampling clock, a new Sample (n) arrives at the Filter input. The new sample is distributed to all the MAC elements simultaneously and applied to one input of each element's multiplier. The other
25 input of each multiplier is that element's coefficient for that time instant, from the coefficient table in the



coefficient generator (Figure 3). Each multiplier's product is then added to that element's accumulator. The input selectors SEL at each element choose which accumulator sum the multiplier product is to be added to: either the
5 element's own accumulator or that of the previous element. Most of the time, between NCO rollovers, the contents of the registers FF are fed back through the selectors SEL to be added to the next product for that MAC element, so that the products are added to the local accumulator. Thus the sum
10 grows in the element's own register FF. But when the NCO rolls over, the selectors SEL select their alternate inputs to cause the sum at each element to be shifted down the chain to the next element in line, with a final sum emerging from the last element in the chain. (For the first MAC element in
15 the chain, the rollover will cause the selector SEL to couple a fixed value to the respective adder, typically zero, though an offset of some value could be entered as desired to overcome some equal and opposite offset in the samples or for some other reason.)

20 In this manner, the final sum is the total of all the elements for the last M periods of the NCO. If T is the number of samples per NCO period, then the total number of samples in the sum, assuming T were constant, would be MT. A final sum emerges at each rollover and these sums represent
25 the rate-converted samples at the new down-sampled rate.



The accumulators must be sized to contain the growth of the accumulating sums caused by both the local accumulation and by the propagation down the chain. The growth from propagation down the chain is bounded not so much by the length of the chain, but by the nature of the Filter's impulse response, that is, by the magnitudes of the coefficients. The growth from the local accumulation is bounded by the maximum amount of rate-reduction intended.

Output Scaling (Figures 1a and 1b)

Each rate-reduced output sample is a sum of a variable number of terms, depending on the ratio of input to output sample rate, that is, the average interval T between NCO rollovers. Because the number of terms is not constant, the gain of the Filter is not constant. Therefore, in order to use this Filter for different output rates, it may be necessary to add a scaling multiplier with an adjustable scale factor to normalize the magnitudes of the output samples over the expected range of output rates.

Timing Recovery Loop Example (Figure 5)

Figure 5 illustrates the use of the Variable-Rate Down-Sampling Filter of the present invention in a timing recovery loop. A fixed-frequency master clock CLK provides timing to the Variable-Rate Down-Sampling Filter and an A/D converter. The Variable-Rate Down-Sampling Filter receives digitized samples from the A/D converter at the sampling frequency F_s .



The Filter's NCO is programmed for a nominal center frequency close to the desired output sample rate F_0 . The Filter performs its rate conversion and filtering functions and outputs samples. It also outputs the NCO rollover signal, whose frequency is F_0 , to be used as a strobe by downstream processing functions, in order to indicate when a rate-converted sample is available.

The converted samples are presented to a timing error detector (such as the well-known zero-crossing detector) which produces as an error signal, an estimate of how far (early or late) from the desired sampling instant the converted samples are. The error signal goes to a loop filter (usually a 1st-order low-pass filter) which accumulates the errors and produces an estimate of the frequency offset from the nominal frequency. This offset is added to the nominal center and presented to the NCO as its Frequency Word, thereby closing the loop.

Derivation

The filters in a demodulation process achieve three purposes:

1. to select the desired signal components and suppress unwanted signals within the sampling bandwidth (anti-aliasing),
2. to equalize or compensate for channel conditions and/or to match the transmit wave-shaping;



3. to interpolate sample values between the actual samples.

The last is the primary function of the Variable-Rate Down-Sampling Filter of the present invention, but

5 incidentally the other two functions can be included at the same time. A suitable filter characteristic (selection of coefficients) can be designed that accomplishes all three purposes. The Filter is based on a finite-impulse-response (FIR) filter architecture which calculates the convolution
10 sum:

$$y(n) = \sum_{i=0}^{DM-1} c(i)x(n-i)$$

where: n = the sampling clock index

$y(n)$ is the output sequence

$x(n)$ is the input sequence

15 $c(i)$ are the coefficients of the filter's impulse response

DM is the total number of coefficients or "taps" in the filter

20 The total number of coefficients is characterized by two parameters D and M in anticipation of reworking the above one-dimensional convolution sum as a two-dimensional sum.

A typical FIR impulse response for a decimate-by- D filter is shown schematically in Figure 6. A shape like this would be used when the desired output rate F_o is equal to the



symbol rate. The nulls are spaced approximately D samples apart and the central lobe contains approximately $2D$ samples. The details of the structure of the impulse response will vary somewhat according to the functions the filter is

5 intended to accomplish. For example, for an output rate F_o at twice the symbol rate (2 output samples per symbol), the lobes would be twice as wide. Furthermore, in a two-channel system where two downsampling filters are driven by the same NCO, the two channels can have different filter responses,
10 for example, shifted in phase for offset-QPSK demodulation. Although the ideal impulse response theoretically extends to infinity, in reality, it is truncated at some suitable length DM , selected for adequate performance.

At each tick n of the sampling clock, a new value $x(n)$
15 is presented to the filter, the entire convolution sum of DM coefficients times the last DM samples is calculated, and an output value $y(n)$ emerges. But if the filter is being used to decimate by D , only 1 out of D outputs are needed and the other $D - 1$ outputs of the D outputs are thrown away. Thus
20 there is no need to calculate the other $D - 1$ outputs. Instead, D samples at a time can be presented to the filter and then the sum is calculated. This simplification lends itself to a structure known as the polyphase structure, shown in Figure 7.

25 As shown in Figure 7, the coefficients are distributed in a matrix, down the columns, then across the rows. There



are D rows or phases; each phase is itself an FIR filter with M coefficients. The commutator steps down the rows, distributing one sample each clock tick to each row. It sweeps out the entire array in D ticks and then recycles; at that time the final sum is computed and a new sample is available at the output.

If it were desired to decimate by less than D, for example by D/N , then the commutator skips N rows and delivers samples only to every Nth phase and zeroes to the others. Again a new output would be available when the commutator recycles. If D/N is a fixed integer, then the commutator will hit the same phases every cycle and the other phases can be eliminated. This is equivalent to scaling the original filter impulse response by decimating it, that is, eliminating all the samples except every Nth. If D/N is not an integer, then the commutator will hit a different set of phases on each pass, but eventually the pattern will repeat. Finally, if D/N is not even constant, the commutator will hit a different set of phases each pass, and the pattern may never repeat exactly. But in all cases, the decimated output is available when the commutator recycles. This is the principle behind the Variable-Rate Down-Sampler. The commutator is the phase index of the NCO, which generates a different set of coefficients for each incoming sample. The recycling of the commutator is the rollover of the NCO at the output sample rate. The polyphase segments are collapsed



into the Coefficient Generator and MAC array as described below.

First the diagram of the polyphase structure is expanded in Figure 8 to show the detail of each phase. Since the phases themselves are FIR filters, they can be implemented in the transpose form as shown in Figure 8. The polyphase representation recasts the one-dimensional sum as a two-dimensional sum:

$$y(n) = \sum_{k=0}^{D-1} \sum_{j=0}^{M-1} c(j, k) x(n - (jD + k))$$

where the original index i has been replaced by the two-dimensional index $(jD+k)$ and the coefficients $c(i)$ have been renumbered with the double index $c(j,k)$. The index j counts cycles of the commutator at rate F_0 and the index k counts the phase within each cycle. Each row of the diagram is a phase and it sums up M samples spaced D apart. Here the D samples $x(n)$ for a F_0 period are spread by the input commutator, one each to the multipliers of each respective FIR filter, multiplied by the applicable coefficient and stored in the respective register FF at the output of the respective multiplier. When the input commutator recycles back to each FIR filter, each new sample for the next F_0 period is multiplied by the same coefficient by the multipliers of the respective FIR filter, added to the contents of the preceding register FF and the result stored in the next register FF. Also on each recycling of the commutator (at the rate F_s/D), the new output $y(n)$,



representing the sum of the last M cycles of the commutator, is available. In essence, Figure 8 presents the detail of Figure 7.

Since addition is commutative, the sums need not be done horizontally first; they can be done vertically first as each sample arrives, and then horizontally when the commutator recycles, as shown in Figure 9. This is nothing more than swapping the order of summation in the two-dimensional sum:

$$y(n) = \sum_{j=0}^{M-1} \sum_{k=0}^{D-1} c(j, k)x(n - (jD + k))$$

But since the commutator hits only one phase at a time, only one row of coefficients, multipliers, and adders is active at one time, the others get zeroes. So each column of multipliers and adders can be collapsed vertically and replaced by a single multiplier and an accumulator. Only the coefficients change with time, so they can come from a lookup table indexed by the commutator-NCO. The horizontal sum on the bottom row occurs at the rollover when each MAC sum is shifted down to its neighbor. The final form of the MAC array part of the Variable-Rate Down-Sampler is shown in Figure 10.

There has been described herein, methods and apparatus for variable-rate down-sampling filters for discrete-time sampled systems using a fixed sampling rate providing variable, non-integral, non-rational, resampling ratio



(F_o/F_s), wherein a continuous range of output sampling rates can be derived from a fixed input sampling rate, wherein the filter characteristics are automatically scaled to the output sampling rate so only one filter set of characteristic needs
5 to be designed, wherein the design can be scaled in number of stages, depth of coefficient tables, and precision of calculations to meet the requirements of the application, and wherein the filter characteristics, stored as coefficients in tables, can be designed to the requirements of the
10 application, for example, a concatenation of anti-aliasing and pre-distortion/equalization functions, all within a modular architecture suited to VLSI implementation.

Thus while preferred embodiments of the present invention have been disclosed and described in detail herein,
15 it will be obvious to those skilled in the art that various changes in form and detail may be made therein without departing from the spirit and scope thereof.



CLAIMS

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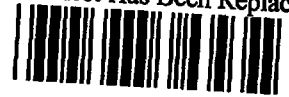


What is claimed is:

1 1. In a digital filter, the improvement comprising:
2 a register having a register input, a register output and a
3 sample clock input;
4 a first-adder having first and second first-adder inputs, a
5 first-adder output and a carry output;
6 a lookup table having an address input and a plurality of
7 filter coefficient outputs;
8 the first first-adder input being coupled to receive a
9 frequency word;
10 the first-adder output being coupled to the register input;
11 the register output being coupled to the address input of the
12 lookup table and to the second first-adder input;
13 the register clock input being coupled to receive a sample
14 clock signal;
15 the first-adder carry output being coupled to provide a
16 rollover signal.

1 2. The improvement of claim 1 wherein the plurality of
2 filter coefficient outputs of the lookup table are each multi-bit
3 outputs.





1 3. The improvement of claim 2 wherein the register and the
2 first-adder are each W bits wide.

1 4. The improvement of claim 3 wherein the address input of
2 the lookup table is P bits wide, wherein P is less than W, and
3 wherein only the P most significant bits of the register output
4 are coupled to the address input of the lookup table, the lookup
5 table storing M times 2^P coefficients, M coefficients at each
6 lookup table address.

1 5. The improvement of claim 4 further comprised of a
2 plurality M of multiplier-accumulator circuits, each multiplier-
3 accumulator circuit being coupled to receive a respective one of
4 each M filter coefficient outputs of the lookup table and a signal
5 sample at the sample clock rate, multiply the same together and
6 accumulate the results in an accumulator, the multiplier-
7 accumulator circuits being coupled in series and responsive to the
8 first-adder carry output to shift the contents of each accumulator
9 in the series of multiplier-accumulator circuits to the
10 accumulator of the next multiplier-accumulator circuit, the
11 contents of the accumulator of the last multiplier-accumulator
12 circuit forming the multiplier-accumulator circuits output.





6. The improvement of claim 5 wherein each multiplier-accumulator circuit comprises:

a multiplier having first and second inputs and an output, a second-adder having first and second inputs and an output, a register having an input, an output and a register clock input, and a selector having first and second inputs and a selector control;

the multiplier having its first input coupled to a respective coefficient output of the lookup table, its second input coupled to receive signal samples and its output coupled to the first input of the second-adder;

the second-adder having its second input coupled to the output of the selector and its output coupled to the input of the register;

the register having its output coupled to the first input to the selector and to the second input to the selector of the next multiplier-accumulator circuit in the series, and its clock input coupled to the sample clock;

the selector having its control coupled to the carry output of the first-adder;

the first multiplier-accumulator circuit in the series having the second input of its selector coupled to an initial value, and the last multiplier-accumulator circuit in the series having the first input of its selector coupled to an output.





1 7. The improvement of claim 2 wherein the lookup table is a
2 RAM.

1 8. The improvement of claim 2 wherein the lookup table is a
2 ROM.

1 9. The improvement of claim 6 wherein the initial value is
2 zero.

1 10. In a digital filter, the improvement comprising:
2 a lookup table having an address input and a plurality of
3 filter coefficient outputs, the address input of the lookup table
4 being P bits wide, the lookup table storing M times 2^P
5 coefficients, M coefficients at each lookup table address;
6 a plurality M of multiplier-accumulator circuits, each
7 multiplier-accumulator circuit being coupled to receive a
8 respective one of each M filter coefficient outputs of the lookup
9 table and a signal sample at a sample clock rate, multiply the
10 same together and accumulate the results in an accumulator, the
11 multiplier-accumulator circuits being coupled in series and
12 responsive to the first-adder carry output to shift the contents
13 of each accumulator in the series of multiplier-accumulator





14 circuits to the accumulator of the next multiplier-accumulator
15 circuit, the contents of the accumulator of the last multiplier-
16 accumulator circuit forming the multiplier-accumulator circuits
17 output.

1 11. The improvement of claim 10 wherein each multiplier-
2 accumulator circuit comprises:

3 a multiplier having first and second inputs and an output, an
4 adder having first and second inputs and an output, a register
5 having an input, an output and a register clock input, and a
6 selector having first and second inputs and a selector control;

7 the multiplier having its first input coupled to a respective
8 coefficient output of the lookup table, its second input coupled
9 to receive signal samples and its output coupled to the first
10 input of the adder;

11 the adder having its second input coupled to the output of
12 the selector and its output coupled to the input of the register;

13 the register having its output coupled to the first input to
14 the selector and to the second input to the selector of the next
15 multiplier-accumulator circuit in the series, and its clock input
16 coupled to the sample clock;

17 the selector having its control coupled to the carry output
18 of the adder;

19 the first multiplier-accumulator circuit in the series having
20 the second input of its selector coupled to an initial value, and





21 the last multiplier-accumulator circuit in the series having the
22 first input of its selector coupled to an output.

1 12. The improvement of claim 11 wherein the lookup table is
2 a RAM.

1 13. The improvement of claim 11 wherein the lookup table is
2 a ROM.

1 14. The improvement of claim 13 wherein the initial value is
2 zero.

1 15. In a digital filter, the improvement comprising:
2 a numerically controlled oscillator responsive to a frequency
3 word and a sample clock to repetitively count through 2^W counts and
4 to output P bits of the count and a carry signal on each
5 completion of the 2^W counts; and,
6 a lookup table having an address input and a plurality of
7 filter coefficient outputs, the address input of the lookup table
8 being P bits wide and being coupled to the P output bits of the
9 numerically controlled oscillator, the lookup table storing M
10 times 2^P coefficients, M coefficients at each lookup table address.





1 16. The improvement of claim 15 wherein P is less than W.

1 17. The improvement of claim 11 wherein the lookup table is
2 a RAM.

1 18. The improvement of claim 11 wherein the lookup table is
2 a ROM.

1 19. In a digital filter, the improvement comprising:
2 first and second multiplier/accumulator units coupled to the
3 same coefficient outputs of the lookup table, each having a
4 plurality of stages coupled in series, each stage having a
5 multiplier responsive to a clock signal for multiplying each of
6 sequential signal inputs by a coefficient provided to the
7 multiplier/accumulator unit, and an accumulator for accumulating
8 the products of the multiplication, the first and second
9 multiplier/accumulator units being responsive to a rollover signal
10 to shift the contents of the accumulator of each stage to the
11 accumulator of the next stage, the last stage of each
12 multiplier/accumulator unit being provided as an output;
13 the first and second multiplier/accumulator units being
14 controllably coupleable in series with the output of the last



15 accumulator of the first multiplier/accumulator unit being
16 provided as the input to the accumulator first second
17 multiplier/accumulator unit, whereby the number of stages coupled
18 in series may be controllably altered.

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1 20. A digital filter comprising:
2 a numerically controlled oscillator responsive to a clock
3 signal and a numerical control signal to advance its count on each
4 clock signal by an amount determined by the numerical control
5 signal, the oscillator providing as outputs, the present
6 oscillator count and a rollover signal each time it counts through
7 a predetermined count;
8 a lookup table having an address input coupled to the present
9 oscillator count output and a plurality of filter coefficient
10 outputs;
11 first and second multiplier/accumulator units coupled to the
12 same coefficient outputs of the lookup table, each having a
13 plurality of stages coupled in series, each stage having a
14 multiplier responsive to the clock signal for multiplying each of
15 sequential signal inputs by a coefficient provided by the lookup
16 table, and an accumulator for accumulating the products of the
17 multiplication, the first and second multiplier/accumulator units
18 being responsive to the rollover signal to shift the contents of
19 the accumulator of each stage to the accumulator of the next
20 stage, the last stage of the multiplier/accumulator units being
21 provided as filter outputs.



1 21. The improvement of claim 20 wherein the lookup table is
2 a RAM.

1 22. The improvement of claim 20 wherein the lookup table is
2 a ROM.

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1 23. A digital filter comprising:
2 a numerically controlled oscillator responsive to a clock
3 signal and a numerical control signal to advance its count on each
4 clock signal by an amount determined by the numerical control
5 signal, the oscillator providing as outputs, the present
6 oscillator count and a rollover signal each time it counts through
7 a predetermined count;
8 first and second lookup tables, each having an address input
9 coupled to the present oscillator count output and a plurality of
10 filter coefficient outputs;
11 first and second multiplier/accumulator units coupled to the
12 coefficient outputs of the first and second lookup tables,
13 respectively, each having a plurality of stages coupled in series,
14 each stage having a multiplier responsive to the clock signal for
15 multiplying each of sequential signal inputs by a coefficient
16 provided by the lookup table, and an accumulator for accumulating
17 the products of the multiplication, the first and second



18 multiplier/accumulator units being responsive to the rollover
19 signal to shift the contents of the accumulator of each stage to
20 the accumulator of the next stage, the last stage of the
21 multiplier/accumulator units being provided as filter outputs.

1 24. The improvement of claim 23 wherein the lookup table is
2 a RAM.

1 25. The improvement of claim 23 wherein the lookup table is
2 a ROM.

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1 26. A method of providing a phase value and a rollover
2 signal in a digital filter comprising:
3 providing a numerically controlled oscillator to count
4 through a predetermined number, and being responsive to a sample
5 clock signal to add a frequency word to the count and to provide a
6 carry signal each time the count exceeds the predetermined number;
7 using the count of the numerically controlled oscillator as a
8 phase value; and,
9 using the carry signal to provide a rollover signal.

1 27. The method of claim 26 wherein the frequency word is
2 variable.





1 28. The method of claim 27 wherein the frequency word is
2 varied responsive to a zero-crossing detector in a timing recovery
3 loop.

1 29. The method of claim 26 further comprised of the steps
2 of:
3 providing a lookup table storing a first plurality of
4 coefficients; and,
5 using the phase value as an address to the lookup table to
6 provide second pluralities of coefficients selected from the first
7 plurality of coefficients responsive to the phase value.

1 30. The method of claim 29 further comprising the steps of:
2 providing a second plurality of accumulators coupled in
3 series;
4 multiplying each coefficient of each second plurality of
5 coefficients by an input sample value and accumulating the sum of
6 each multiplication in a respective one of the accumulators;
7 shifting the accumulated sum in each accumulator to the next
8 accumulator in the series responsive to the rollover signal, and
9 providing the sum in the last of the second plurality of
10 accumulators as an output sample.

