

Description

BACKGROUND OF THE INVENTION

This invention relates generally to a semiconductor integrated circuit (IC) device. More particularly, the present invention relates to semiconductor circuit technique which is effective when applied, for example, to a semiconductor memory device incorporating therein a substrate bias generation circuit such as a dynamic RAM (Random Access Memory).

In semiconductor memory devices constituted by MOSFETs (Insulated Gate type Field Effect Transistors), it is known in the art to generate a substrate back-bias voltage by a built-in substrate back-bias generation circuit in order to reduce the parasitic capacitance between circuit elements such as MOSFETs and a semiconductor substrate. For example, refer to "Nikkei Electronics", May 14, 1979, p.p. 77 - 79, published by Nikkei McGraw Hill Co.) When such a substrate bias generation circuit is incorporated, a power source voltage to be supplied to a semiconductor memory device can be unified to a voltage such as 5 V, and the number of external terminals therefor can be reduced.

As a result of studies, however, the inventors of the present invention have found that if a circuit for rectifying the output pulses generated continuously by an oscillation circuit is used in this case, the following problem develops. A current flowing to the substrate varies greatly between the accessing state in which each circuit starts operating simultaneously and the non-accessing state in which no internal circuit operates. Therefore, when the substrate back-bias voltage is generated by rectifying those oscillation pulses that are generated in no relation to circuit operation, the current supply capacity is essentially set in a "worst case" condition. This requires relatively large capacitor and rectification elements and a driving circuit, so that the integration density of the semiconductor integrated circuit is reduced. In addition, more current is drawn. (For details of the substrate bias generation circuit, refer to Japanese Patent Laid-Open No. 13566/1980, for example).

GB-A-2 111 336, EP-A-0 118 108 the latter being cited under Art.54(3)EPC, disclose a semiconductor integrated circuit with the features set forth in the first part of claim 1. In the known circuits the back-bias voltage is controlled in synchronism with the operation of the circuit elements included in the integrated circuit to which the back-bias voltage is applied.

IBM Technical Disclosure Bulletin (Vol. 22, no. 7, Dec. 1979, p. 2765-2767) discloses a level detection circuit (threshold detector) for detecting the

level of a back-bias voltage (substrate bias voltage), wherein the output signal (VOUT) of the level detection circuit controls the back-bias voltage generator to increase the back-bias voltage if the back-bias voltage level is detected to be insufficient.

It is an object of the present invention to provide a semiconductor integration circuit in which the back-bias voltage generation circuit is additionally utilized to prevent an increase of the leakage current due to temperature variations.

This object is met by the invention characterized in claim 1.

BRIEF DESCRIPTION OF THE DRAWINGS

Fig. 1 is a circuit diagram showing one embodiment of the present invention;

Fig. 2 is a circuit diagram showing an example of the substrate back-bias voltage generation circuit of the embodiment shown in Fig. 1;

Fig. 3 is a timing chart useful for explaining the operation of the substrate back-bias voltage generation circuit;

Fig. 4 is a circuit diagram showing another embodiment of the present invention; and

Figs. 5 and 6 are circuit diagrams showing other embodiments of the present invention, respectively.

DESCRIPTION OF THE PREFERRED EMBODIMENTS[Embodiment 1]

Fig. 1 is a circuit diagram showing a dynamic RAM in accordance with one embodiment of the present invention. Each circuit element or each circuit block shown in the circuit diagram is formed on one semiconductor substrate such as single crystal silicon by a heretofore known production technique for semiconductor integrated circuits, though not particularly limited to that configuration. Various MOSFETs formed on the semiconductor substrate are in the enhancement mode. (This also applies to the other embodiments of the invention to be described later.)

A memory array MARY comprises of a plurality of memory cells arranged in a matrix, a plurality of data lines DL, DL and a plurality of word lines. Though not particularly limited to that configuration, the memory array MARY is of a folded bit line (data line) construction.

Each of the memory cells MC comprises of a data storage capacitor C_s , one of the electrodes of which is connected to a reference potential point such as a power terminal of the circuit, and an address selection MOSFET Q_m interposed between this capacitor C_s and the data line. Logic "1"

and "0" stored in the memory cells are corresponded whether a charge is stored in the capacitor.

In the data read-out operation, each data line DL, $\overline{DL}$ of the memory array MARY is first pre-charged by a pre-charge circuit PC to a level substantially close of the power source voltage V_{cc} of the circuit. The pre-charge circuit PC comprises, for example, of pre-charge MOSFETs Q_{c1} and Q_{c2} that are interposed between the data lines DL, $\overline{DL}$ and the power terminal V_{cc} , respectively. The conduction of these precharge transistors MOSFETs Q_{c1} and Q_{c2} is controlled by a pre-charge pulse ϕ_{pc} . The pre-charge circuit PC may include an equalizer MOSFET that is interposed between the pair of data lines DL, $\overline{DL}$ and is controlled by the pre-charge pulse ϕ_{pc} , in addition to the pre-charge MOSFETs Q_{c1} and Q_{c2} .

One of the plurality of word lines WL of the memory array MARY is selected after each data line has been pre-charged. When a particular word line is selected, the MOSFET Q_m of the memory cell corresponding to the selected word line is turned on and the capacitor C_s is coupled to the data line DL or $\overline{DL}$. Accordingly, the potential of the data line DL or $\overline{DL}$ to which the memory cell is connected is changed. The potential of the data line DL or $\overline{DL}$ in this case is changed in accordance with the charge quantity stored in the capacitor C_s . This potential change of the data line is sensed by a sense amplifier SA.

In a memory array having a large capacity, each memory is fabricated so as to be smaller, and a large number of memory cells are coupled to the respective data lines DL, $\overline{DL}$. Therefore, the ratio C_s/C_o of the capacitor C_s to the stray capacity C_o - (not shown) of the common data line DL is extremely small. This means that the potential change applied to the data line DL or $\overline{DL}$ in response to the charge stored in the capacitor C_s , that is, a signal, is extremely weak.

Though not particularly limited to this configuration, this embodiment includes one dummy cell DC for each data line in the same way as in the well known dynamic RAM in order to detect such a weak signal. The dummy cell DC is fabricated under the same production conditions and with the same design constants as those of the memory cell MC except that the capacity of the capacitor C_D of the dummy cell DC is half that of the capacitor C_s of the memory cell MC. Before addressing, the capacitor C_D is charged to ground potential by an MOSFET Q_d , that receives a timing signal ϕ_d . Since the capacitance of the capacitor C_D is half that of the capacitor C_s , the capacitor C_D applies a reference voltage, which is substantially half of the read-out signal from the memory cell MC, to the corresponding data line.

In the circuit diagram, the symbol SA represents a sense amplifier which amplifies the difference of such potential changes caused by addressing within a sense period that is determined by timing signals (sense amplifier control signals) ϕ_{pa1} , ϕ_{pa2} . (The operation of the sense amplifier will be described after.) The input and output nodes of the sense amplifier are coupled to a pair of complementary data lines DL and $\overline{DL}$ that are arranged in parallel with each other. The number of the memory cells that are connected to these complementary data lines DL, $\overline{DL}$, respectively, are made to be equal in order to improve the data detection accuracy at the time of the data read-out operation.

When the memory cells MC connected to one of the complementary data lines DL, $\overline{DL}$ are selected during addressing, one of a pair of dummy word lines DWL, $\overline{DWL}$ is selected so that the dummy cells connected to the other of the data lines are selected correspondingly.

The sense amplifier SA includes a pair of MOSFETs Q_1 , Q_2 whose gates and drains are cross-connected, and differentially amplifies a weak signal appearing across the complementary data lines DL, $\overline{DL}$ by these MOSFETs. This amplification operation is divided into two stages by an MOSFET Q_7 having relatively small conductance and an MOSFET Q_8 having relatively large conductance. When the MOSFET Q_7 is rendered conductive by a relatively quick timing signal ϕ_{pa1} , the amplification operation of the first stage is actuated in response thereto, and the amplification of the second stage is started at the time at which the potential difference between the complementary data lines DL, $\overline{DL}$ becomes great to a certain extent and a timing signal ϕ_{pa2} is generated. In other words, when the MOSFET Q_8 is rendered conductive by the timing signal ϕ_{pa2} , the amplification operation of the second stage is started in response thereto. The two stage operation of the sense amplifier SA makes it possible to effect amplification devoid of any error of the potential difference between the complementary data lines DL, $\overline{DL}$ and to effect amplification at a higher operating speed. As a result of the amplification operation by the sense amplifier SA, one of the pair of data lines is set to a potential somewhat lower than the power source voltage V_{cc} while the other is set to a low potential substantially equal to the ground potential (0 V) of the circuit.

The stored data of the memory cell, which is once about to be destroyed when addressing is effected, is restored as the high or low level potential obtained by this sense operation is as such supplied to the memory cell MC. In other words, the stored data that has temporarily been read out is written once again into the memory cell.

An active restore circuit AR is disposed between the complementary data lines DL and $\overline{DL}$ in order to raise the high level potential re-written into the memory cell MC to a level that is substantially equal to the power source voltage V_{cc} of the circuit. This active restore circuit AR has the function of selectively boosting only the high level signal to the power source voltage V_{cc} without affecting at all the low level signal. The explanation in detail of the definite circuit construction of this active restore circuit AR is omitted hereby because it is not directly relevant to the gist of the present invention.

A column switch CW comprising of MOSFETs Q_3 and Q_4 is interposed between the pair of data lines DL, $\overline{DL}$ and the pair of common complementary data lines CDL, $\overline{CDL}$. Similarly, another column switch CW comprising of a similar MOSFETs Q_5 and Q_6 is interposed between the other data line pair and the common complementary data line pair $\overline{DL}$, $\overline{CDL}$. The input terminals of a data output buffer DOB including an output amplifier and the output terminal of a data input buffer DIB are connected to the common complementary data line pair CDL, $\overline{CDL}$.

A row decoder R-DCR and a column decoder C-DCR receive internal complementary address signals generated by address buffers R-ADB and C-ADB, and generate a selection signal for selecting one word line and one dummy word line as well as a column switch selection signal to be applied to the column switches. Addressing to the memory cells and to the dummy cells is effected in this way.

The operations of the address buffers R-ADB and C-ADB are controlled by timing signals ϕ_{ar} and ϕ_{ac} , respectively, and the operations of the row and column decoders R-DCR and C-DCR are controlled by timing signals ϕ_x and ϕ_y , respectively. In other words, external address signals $AX_0 - AX_1$ are taken in by the row address buffer R-ADB in synchronism with the timing signal ϕ_{ar} that is formed on the basis of a row address strobe signal $\overline{RAS}$, and the internal address signals generated by the address buffer R-ADB are transferred to the row decoder R-DCR. The address decoder R-DCR decodes the internal address signal supplied from the row address buffer ADB, and sets one word line and one dummy word line to a selection level at a timing in accordance with a word line access timing signal ϕ_x .

External address signals $AY_0 - AY_1$ are taken in by the column address buffer C-ADB in synchronism with the timing signal ϕ_{ac} formed on the basis of the column address strobe signal $\overline{CAS}$ and are transferred to the column decoder C-DCR. The column decoder C-DCR generates a column selection signal for selecting a predetermined data line at the timing in accordance with a data line selec-

tion timing signal ϕ_y .

A timing control circuit TC receives the row address strobe signal $\overline{RAS}$, the column address strobe signal $\overline{CAS}$ and a write enable signal $\overline{WE}$ that are supplied from external terminals, and generates various timing signals necessary for the memory operation besides the timing signals described above as the typical examples.

The address buffer, address decoder and data output buffer DOB of the column system comprise CMOS (complementary MOS) type static circuits, though they are not particularly limited to this configuration in order to accomplish the lower power consumption of the device and to accomplish continuous read-out operations by bringing the word lines into the accessing state and changing over the column address signals.

A substrate bias generation circuit V_{bb} -G is actuated by a positive power source voltage such as 5 V that is applied across the power terminal V_{cc} as one of the external terminals of the integrated circuit and the reference potential terminal (or the ground terminal) GND, and generates a negative bias voltage.

The bias voltage produced from the substrate bias generation circuit V_{bb} -G is supplied to semiconductor regions which act as a common substrate gate of MOSFET Q_m in the memory array and MOSFETs constituting the circuit blocks shown in the drawing.

The CMOS integrated circuit of this embodiment is formed on the semiconductor substrate which consists of single crystal P-type silicon, but it is not particularly limited to this configuration.

Though not particularly limited to this configuration, an N-channel MOSFET such as MOSFET Q_m in the memory array MARY is constructed from an N-type source region and an N-type drain region, both formed on the surface of the semiconductor substrate, and a gate electrode which is formed on the surface of the semiconductor substrate between the source region and the drain region via a thin gate insulating film, and which comprises of polysilicon. A P-channel MOSFET is formed on an N-type well region formed on the surface of the semiconductor substrate. Thus, the semiconductor substrate constitutes a common substrate gate for a plurality of N-channel MOSFETs formed thereon. The N-type well region constitutes the substrate gate of the P-channel MOSFET formed thereon. The substrate gate of the P-channel MOSFET, that is, the N-type well region, is coupled to the power terminal V_{cc} of Fig 1.

Among the main surface of the semiconductor substrate, the surface portions other than the surface portions to serve as the active regions, that is, the surface portions other than the surface portions on which MOSFETs, MOS capacitors and semicon-

ductor wiring regions are to be formed, are covered by a relatively thick field insulating film, though the film is not shown in the drawing. The necessary wiring layer is extended onto the field insulating film or is extended onto the active regions via an insulating film.

According to the construction described above, the back-bias voltage $-V_{bb}$ produced from the substrate bias generation circuit V_{bb} -G is supplied to the common substrate gate of the N-channel MOSFETs formed on the surface of the semiconductor substrate.

The back-bias voltage reduces the junction capacitance formed by the P-N junction between the source-drain regions of the N-channel MOSFETs and the semiconductor substrate and by the P-N junction between the semiconductor wiring regions and the semiconductor substrate. Since the parasitic capacitance which limits the operating speed is thus reduced, the integrated circuit can operate at a higher speed.

MOSFETs such as the address selection MOSFETs Q_m sometimes generate a tailing current or leakage current even when they are turned off. The threshold voltage of the MOSFET is increased suitably due to the substrate bias effect when the back-bias voltage $-V_{bb}$ is applied, so that the leakage current decreases. Since the leakage current of the address selection MOSFET Q_m is reduced, the retention time of the charge stored in the data storage capacitor C_s is relatively prolonged.

A structure of an integrated circuit consisting of a field insulating film and a wiring layer such as a signal wiring layer extending on the field insulating film can be regarded as constituting a part of the parasitic MOSFET structure. The back-bias voltage $-V_{bb}$ increases the threshold voltage of the parasitic MOSFET and prevents the operation of the parasitic MOSFET.

As is well known in the art, the proportion of the increase of the threshold voltage of MOSFET due to the substrate bias effect decreases with a higher substrate bias voltage. Therefore, the threshold voltage of each N-channel MOSFET remains within a relatively narrow range when the back-bias voltage $-V_{bb}$ is generated, irrespective of the variance of the characteristics of the MOSFETs resulting from the variance developing during the fabrication of the integrated circuit.

As will be more obvious from the description appearing later, the substrate bias generation circuit V_{bb} -G periodically generates the bias voltage due to the charge pump action utilizing the capacitor. The back-bias voltage is smoothed by the parasitic capacitance and the stray capacitance that exist between the semiconductor substrate to which it is applied, and the power source wiring layer, the semiconductor regions, and the like,

The back-bias voltage which is retained substantially by the capacitance is reduced by a leakage current that develops between the source-drain region of MOSFET and the semiconductor substrate.

Here, the leakage current for the semiconductor substrate is not always constant, but is affected by the circuit operation. This leakage current is relatively small so long as the switching state of MOSFET remains unaltered and is kept fixed or stationary. Conversely, if the switching state of MOSFET changes, the leakage current is increased by such a change. For details of the mechanism of occurrence of the leakage current to the substrate, see "Physics of Semiconductor Devices", p.p. 480 - 487 by S. M. Sze, published by John Wiley & Sons, 1981.

In the dynamic RAM shown in Fig. 1, the substrate leakage current increases when the timing control circuit TC, the address buffers, the decoders, the sense amplifier and the like operate on the basis of the row address strobe signal RAS , the column address strobe signal CAS , and the like.

In accordance with this embodiment, the substrate bias generation circuit V_{bb} -G has a relatively large driving capacity so that it can keep the substrate bias potential at a suitable value even when the substrate leakage current increases. The circuit V_{bb} -G is also designed so as to exhibit low power consumption characteristics.

Though not particularly limited to this configuration, the substrate bias generation circuit V_{bb} -G of this embodiment includes a circuit portion exhibiting a steady operation and a circuit portion exhibiting an intermittent operation, from the aspect of its driving capacity and its power consumption. The circuit portion exhibiting the steady operation is provided with the driving capacity such that when each circuit shown in Fig. 1 is substantially in the non-operating state, it can keep the back-bias voltage $-V_{bb}$ at a desired value.

The circuit portion exhibiting the intermittent operation is provided with a relatively large driving capacity so that the back-bias voltage can be kept at desired values even when the substrate leakage current is increased.

A level detection circuit VLD such as shown in Fig. 1 is provided in order to control the operation of the circuit portion exhibiting the intermittent operation. the level detection circuit VLD detects the back-bias voltage $-V_{bb}$, and produces a signal for operating the circuit portion of the intermittent operation when the back-bias voltage is lower than a desired level.

Though not particularly limited to this configuration, the operation of the circuit portion exhibiting intermittent operation in the substrate bias genera-

tion circuit in accordance with this embodiment is also controlled by a relatively fast row system control signal RAS_1 which is produced from the timing control circuit TC on the basis of the external control signal RAS .

This construction makes it possible to obtain the following circuit operations.

When the access to the dynamic RAM of this embodiment is started by the row address strobe signal RAS , the circuits shown in the drawing start operating in response thereto, and the substrate leakage current therefore increases. The level of the back-bias voltage $-V_{bb}$ becomes lower with an increasing substrate leakage current. In this case, the back-bias voltage is controlled in such a manner as to again assume the desired level by a feedback route consisting of the level detection circuit VLD and the circuit portion exhibiting the intermittent operation, even when the operation control of the substrate bias generation circuit by the control signal RAS_1 does not exist. In this case, however, the time required before the back-bias voltage returns to the desired level becomes somewhat long in accordance with the change of speed of the output of the circuit portion exhibiting the intermittent operation.

Conversely, when the control signal RAS_1 , that is, the control signal having a quicker timing among the row system control signals produced from the timing control circuit TC, is utilized as in this embodiment, the operation of the circuit portion exhibiting intermittent operation can be started at the timing which is substantially the same as the timing at which the substrate leakage current is drastically increased. As a result, the drastic level change of the back-bias voltage can be prevented.

When the circuit portion of the substrate bias generation circuit V_{bb} -G exhibiting the intermittent operation is controlled by a control signal such as the control signal RAS_1 , the level detection circuit VLD can be omitted. However, the following must be taken into consideration in such a case.

It is preferred that the back-bias voltage can change from 0 volt to the desired level within a relatively short period after the power source has been turned on. To speed up the generation of the back-bias voltage at the time the power source is turned on, it becomes necessary that the circuit portion exhibiting the intermittent operation in the substrate bias generation circuit V_{bb} -G be also operated. For this purpose, the row address strobe signal for executing the dummy operation cycle must be applied to the external terminal RAS at the same time that the power is turned on.

When the detection output of the level detection circuit VLD is utilized, the circuit portion exhibiting the intermittent operation is immediately rendered operative by the detection output, so that the

back-bias voltage is changed to the predetermined level within a relatively short period from the time that the power source is turned on, irrespective of the signal applied to the external terminal RAS .

When the output of the level detection circuit VLD is not utilized, the level of the back-bias voltage might be reduced undesirably due to the increase of the substrate leakage current resulting from the rise of the operating temperature of the integrated circuit.

Fig. 2 is a circuit diagram showing an example of the substrate bias generation circuit V_{bb} -G together with that of the level detection circuit VLD described above. In this circuit diagram, those MOSFETs which are provided with straight lines between their sources and drains are of the P-channel type, while those MOSFETs which are expressed by ordinary symbols are of the N-channel type.

In this embodiment, two kinds of substrate back-bias voltage generation circuits, that is, a substrate bias voltage generation circuit V_{bb} -G1 constituting the circuit portion of the steady operation and a substrate bias voltage generation circuit V_{bb} -G2 constituting the circuit portion of the intermittent operation, are provided. The back-bias voltage generation circuit V_{bb} -G1 of the steady operation comprises of an oscillation circuit OSC2, CMOS inverter circuits IV4, IV5 for waveform shaping and amplifying the output of the oscillation circuit and a rectification circuit.

The oscillation circuit OSC2 comprises for example, of a ring oscillator which is operated by the power source voltage V_{cc} and comprises of a plurality of CMOS inverter circuits that are coupled with one another in a ring configuration.

The rectification circuit comprises of a charge pump capacitor C2 and MOSFETs Q_{20} , Q_{21} whose gate electrodes are connected to their drain electrodes (which operate either as the drain electrodes or as the source electrodes depending upon the polarity of the voltage applied thereto, but are called hereby the drain electrodes) so that the transistors function as the rectification elements. Though not particularly limited to this configuration, the capacitor C2 has an MOS capacitor structure having a similar structure to the N-channel MOSFET. In other words, one of the electrodes of the capacitor which should correspond to the gate electrode of the MOSFET is coupled to the output terminal of the CMOS inverter circuit IV5 as the output buffer. The other of the electrodes of the capacitors C2, that is, the electrode that should correspond to the source or drain electrode of the MOSFET, is coupled to the common junction between the MOSFETs Q_{20} and Q_{21} .

The MOSFET Q_{20} which acts as the rectification element is interposed between the other elec-

trode of the capacitor C_2 and the grounding point GND of the circuit, and the MOSFET Q_{21} is disposed between the other electrode of the capacitor C_2 and the semiconductor substrate.

A parasitic capacitance C_{sb} (not shown), that retains substantially the back-bias voltage, exists between the substrate and the grounding point of the circuit.

The MOSFET Q_{20} of the diode form is turned on when the oscillation pulse produced from the inverter circuit IV5 is at the high level (substantially at the level of the power source voltage V_{cc}), and the capacitor C_2 is pre-charged by the output high level. Next, when the output pulse is at the low level (substantially at the level of the ground potential of the circuit), the other electrode of the capacitor C_2 is at a negative potential of $-(V_{cc} - V_{th})$. Here, the symbol V_{th} represents the threshold voltage of the MOSFET Q_{20} . The MOSFET Q_{21} of the diode form is turned on by this negative potential and transmits the negative potential to the parasitic capacitance C_{sb} described above. Therefore, the substrate bias voltage $-V_{bb}$ is applied to the substrate. The substrate bias voltage generation circuit V_{bb} -G1 of the steady operation has a relatively small current supply capacity such that when the RAM described above is under the chip non-selection state, it can compensate for the leakage current flowing through the substrate.

The current supply capacity of the substrate bias voltage generation circuit V_{bb} -G1 of the steady operation is determined substantially by the capacitance of the capacitor C_2 and the oscillation frequency of the oscillation circuit OSC. In other words, the quantity of the charge injected into the semiconductor substrate in response to one oscillation output becomes greater with a greater capacitance of the capacitor C_2 . The number of times of the charge injection into the semiconductor substrate per unit time becomes greater with a higher oscillation frequency of the oscillation circuit OSC₂.

In accordance with this embodiment, the substrate bias voltage generation circuit of the steady operation is constituted in such a fashion as to exhibit low power consumption characteristics while securing a necessary and relatively small current supply capacity. The oscillation frequency of the oscillation circuit OSC₂ is set to be a relatively low value such as 1 or 2 MHz by selecting a suitable number of CMOS inverter circuits forming the oscillation circuit and by setting their signal delay characteristics to suitable levels.

Here, the power consumed by the oscillation circuit OSC₂ is proportional to the oscillation frequency. The operation current or consumed current of each CMOS inverter circuit constituting the oscillation circuit OSC₂ is proportional to a so-called "transient current" necessary for the charge and

discharge of the load capacitance (consisting of wiring capacity, input capacitance of inverter circuits of the post stage and the like) coupled to the output of each inverter circuit in the same way as in the well known CMOS inverter circuit, and is substantially zero in the stationary state in which the output or input of each inverter is at the high or low level. Since the transient current of each CMOS inverter circuit is proportional to the operation frequency, the power consumption of the oscillation circuit OSC₂ having a low oscillation frequency is low.

In accordance with this embodiment, the driving capacity of the CMOS inverter circuit IV₅ as the output buffer for driving the rectification circuit may be relatively small because the capacitor C_2 is relatively small. Therefore, the P- and N-channel MOSFETs, not shown, constituting this CMOS inverter circuit IV₅ need not have low ON resistance; hence, may be small. The P- and N-channel MOSFETs, not shown, constituting the CMOS inverter circuit IV₄ as the waveform shaping circuit need only drive a load having a relatively small capacitance because the MOSFETs constituting the CMOS inverter circuit IV₅ are small. Therefore, the MOSFETs constituting the CMOS inverter circuit IV₄ may be small.

The substrate bias generation circuit V_{bb} -G2 for intermittent operation comprises of a controllable oscillation circuit, that is, an oscillation circuit OSC₁ capable of the intermittent operation, a CMOS inverter circuit IV₂ as a waveform shaping circuit, a CMOS inverter circuit IV₃ as an output buffer and a rectification circuit.

Though not particularly limited to this configuration, the oscillation circuit OSC₁ comprises of CMOS NAND gate circuits G_2 through G_4 . The output terminals of these gate circuits $G_2 - G_4$ are connected to one of the input terminals of a gate circuit of the post stage. The output terminal of the gate circuit G_4 of the final stage is connected to one of the input terminals of the gate circuit G_2 of the initial stage. The other input terminal of each of the gate circuits $G_2 - G_4$ is regarded as a common operation control terminal and is connected to the output terminal of the gate circuit G_1 .

Each of the gate circuits $G_2 - G_4$ constituting the oscillation circuit OSC₁ operates substantially as an inverter when the control signal supplied to the operation control terminal is at the high level (logic "1") such as one that is substantially equal to the power source voltage V_{cc} . Therefore, the oscillation circuit OSC₁ performs the oscillation operation as a ring oscillator. When the control signal is at the low level (logic "0") such as one that is substantially equal to the ground potential, the output of each of the gate circuits $G_2 - G_4$ is kept fixed at the high level which is substantially equal

the power source voltage V_{cc} .

The rectification circuit comprises of a capacitor C_1 and MOSFETs Q_{18} , Q_{19} as shown in the drawing.

When oscillation circuit OSC_1 is rendered operative by the high level of the control input, the rectification circuit comprising of the capacitor C_1 and the MOSFETs Q_{18} , Q_{19} is operated in response to the former, and the charge for applying a back-bias voltage is injected into the semiconductor substrate. The back-bias voltage in this case is determined by the substrate bias voltage generation circuit $V_{bb}-G_1$ of the steady operation with the substrate bias voltage generation circuit $V_{bb}-G_2$.

When the oscillation circuit OSC_1 is rendered inoperative by the low level of the control input, the rectification circuit comprising of the capacitor C_1 and the MOSFETs does not operate. In this case, the output of the CMOS inverter circuit IV_3 is kept at the high level substantially equal to the power source voltage V_{cc} by the high level output of the oscillation circuit OSC_1 . The capacitor C_1 is kept in the charge state by the high level output of the inverter IV_3 . This construction makes it possible to inject the charge into the substrate at an early timing when the oscillation circuit OSC_1 starts operating.

The CMOS NAND gates $G_2 - G_4$ constituting the oscillation circuit OSC_1 do not consume current so long as they are in the stationary state, in the same way as the CMOS inverter circuit. Therefore, the power consumed by the substrate bias voltage generation circuit $V_{bb}-G_2$ of the intermittent operation is substantially zero during the period in which the oscillation circuit OSC_1 stops operating.

The substrate back-bias voltage generation circuit $V_{bb}-G_2$ operating intermittently must have a relatively large current supply capacity so that it can compensate for a relatively large leakage current that flows to the substrate when the RAM is in the operative state. Therefore, the capacitance of the capacitor C_1 is relatively large, while the oscillation frequency of the oscillation circuit OSC_1 is relatively large such as from 10 to 15 MHz.

The P- and N-channel MOSFETs, not shown, that constitute the CMOS inverter circuit IV_3 are relatively large because the rectification circuit constitutes a relatively heavy load. The P- and N-channel MOSFETs, not shown, that constitute the CMOS inverter circuit IV_2 are relatively large so that they can sufficiently drive the CMOS inverter circuit IV_3 .

This embodiment includes a level detection circuit VLD comprising of MOSFETs $Q_{10} - Q_{17}$ and CMOS inverter circuits IV_0 , IV_1 , and a control circuit comprising of the CMOS NAND gate circuit G_1 in order to operate the substrate bias voltage generation circuit $V_{bb}-G_2$ only when the operation is

necessary.

The level detection circuit VLD is provided in order to positively detect excess substrate back-bias voltage $-V_{bb}$ beyond a predetermined level necessary for high speed operation of the RAM. In the level detection circuit VLD, the ground potential of the circuit is steadily applied to the gate of the P-channel MOSFET Q_{10} so that the transistor serves as a constant current load. In other words, the MOSFET Q_{10} is constantly turned on. A P-channel MOSFET Q_{11} for level clamping is connected in series with this MOSFET Q_{10} . Since the ground potential of the circuit is constantly applied to the gate, this MOSFET Q_{11} is constantly kept ON. Therefore, the source potential of the MOSFET Q_{11} , that is, the potential of the electrode coupled to the drain of the MOSFET Q_{10} , is at the level which is higher than at least the ground potential of the circuit, and the drain potential is substantially equal to the ground potential of the circuit. MOSFETs $Q_{12} - Q_{14}$ in the diode form are connected in series between the drain of the MOSFET Q_{11} and the substrate ($-V_{bb}$).

Therefore, the detection level of the level detection circuit VLD is substantially equal to the sum $3V_{th}$ of the threshold voltages V_{th} of the three MOSFETs Q_{12} through Q_{14} connected in series. If the substrate back-bias voltage $-V_{bb}$ is at the level lower than the total threshold voltage $3V_{th}$ of the three transistors $Q_{12} - Q_{14}$ in the diode form, these transistors are turned off. In this case, the potential at the junction between the MOSFETs Q_{11} and Q_{10} is at the high level such as the power source voltage V_{cc} . If the substrate back-bias voltage $-V_{bb}$ is at the level higher than the level of the total threshold voltage $3V_{th}$ of the MOSFETs $Q_{12} - Q_{14}$ in the diode form, these transistors $Q_{12} - Q_{14}$ are turned on. In this case, the potential at the junction between the MOSFETs Q_{11} and Q_{10} is at the low level which is higher by the threshold voltage V_{th} of the MOSFET Q_{11} than the ground potential of the circuit. In this case, the current flowing from the power source terminal V_{cc} to the substrate positively reduces the substrate back-bias voltage $-V_{bb}$.

The conductance of the load MOSFET Q_{10} is set to an extremely small value in order to minimize the current flowing to the substrate through the level detection circuit and to sufficiently reduce the low level appearing at the junction between the MOSFETs Q_{10} and Q_{11} . In other words, the conductance is set to an extremely small conductance so that the MOSFET Q_{10} permits the flow of only a slight current.

The high and low levels of the detection output such as described above are judged by a CMOS inverter circuit constituted by a P-channel MOSFET Q_{15} and an N-channel MOSFET Q_{16} . Though not particularly limited to this configuration, the inverter

circuit comprising of the MOSFET Q_{15} and Q_{16} forms a Schmidt circuit (hysteresis circuit) together with an MOSFET Q_{17} and a CMOS inverter circuit IV_0 in order to realize a high speed change of the detection output to be obtained and particularly, to operate the oscillation circuit OSC_1 rapidly when the back-bias voltage is reduced. In other words, the output of the inverter circuit comprising of the MOSFETs Q_{15} and Q_{16} is applied to the input of the CMOS inverter circuit IV_0 having a similar construction. The output of this CMOS inverter circuit IV_0 is applied to the gate of the P-channel MOSFET Q_{17} disposed between its input and the power source voltage V_{cc} , thereby effecting positive feedback. When the low level detection output is formed, the detection signal produced from the inverter circuit IV_0 is changed to the low level at a high speed. The detection output generated by this inverter circuit IV_0 is applied to one of the input terminals of the CMOS NAND gate circuit G_1 through the CMOS inverter circuit IV_1 . The internal row address strobe signal $\overline{RAS}$ formed by the timing control circuit TC shown in Fig. 1 is applied to the other input terminal of this NAND gate circuit G_1 . The output of this NAND gate circuit G_1 is applied in common to the other input terminals of the NAND gate circuits $G_2 - G_4$ that constitute the ring oscillator OSC_1 described above.

Next, the operation of the circuit of this embodiment will be described with reference to the timing chart of Fig. 3.

When the RAM is in the chip non-selecting state or when the internal address strobe signal $\overline{RAS}$ is at the high level, the output of the gate circuit G_1 responds to the detection output of the level detection circuit VLD.

Under this chip non-selecting state, if the absolute value of the substrate back-bias voltage $-V_{bb}$ is less than that of the total threshold voltage $3V_{th}$ of the three MOSFETs Q_{12} through Q_{14} described already, these transistors are turned off; hence, the detection output is at the high level. Therefore, the detection output supplied to the NAND gate circuit G_1 is at the low level (logic "0"), and the output of the NAND gate circuit G_1 is at the high level (logic "1"), whereby the oscillation circuit OSC_1 is in the oscillating state. The absolute value of the substrate back-bias voltage is increased by the rectification circuit that receives the output pulses of the oscillation circuit. When the substrate back-bias voltage $-V_{bb}$ exceeds the total threshold voltage $3V_{th}$, the MOSFETs $Q_{12} - Q_{14}$ are turned on, so that the detection output is at the low level, whereupon the detection output supplied to the NAND gate circuit G_1 is at the high level (logic "1"). Since the output of the NAND gate circuit G_1 falls to the low level (logic "0") in response to the former, the outputs of all the NAND gate circuits $G_2 - G_4$

constituting the oscillation circuit OSC rise to the high level (logic "1"). In other words, oscillation stops.

Since oscillation stops, the operation of the rectification circuit (C_1 , Q_{18} , Q_{19}) also stops. Since the oscillation circuit consuming much power and the rectification circuit thus stop operating, lower power consumption can be accomplished. Incidentally, since the substrate back-bias voltage is at a low level at or near ground potential immediately after turning on the power, the operations of both substrate back-bias voltage generation circuits can quickly raise the absolute value of the substrate back-bias voltage to the desired level.

When the row address strobe signal $\overline{RAS}$ falls to the low level and chip selecting is thus indicated, the internal signal $\overline{RAS}$ is lowered to the low level in response thereto, so that the output of the NAND gate circuit G_1 rises to the high level (logic "1") irrespective of the detection output of the level detection circuit described above. When the RAM executes the write-in/read-out operations and the like, the oscillation circuit OSC_1 is rendered unconditionally operative. This is to prevent the drastic drop of the absolute value of the substrate back-bias voltage $-V_{bb}$ that is caused by a relatively great substrate leakage current occurring when RAM operations such as described above are started. If the oscillation circuit OSC_1 is rendered operative in advance before the RAM is rendered operative as in this embodiment, it becomes possible to prevent the drastic drop of the substrate back-bias voltage $-V_{bb}$.

[Embodiment 2]

Fig. 4 is a circuit diagram showing a dynamic RAM in accordance with the second embodiment of the invention. Those circuits which are not shown in Fig. 4 are substantially the same as those shown in Fig. 1.

The RAM in this embodiment includes a refresh control circuit REFC and a multiplexer MPX to accomplish the automatic refresh of memory cells.

The refresh control circuit REFC includes a refresh timer and a refresh address counter that are not shown.

The refresh timer is operated when the row address strobe signal $\overline{RAS}$ is raised to the high level and the refresh control signal REFH is lowered to the low level, that is, when the refresh operation is indicated in the chip non-selecting state, and produces periodically refresh control signals ϕ_{ref} during its operation.

The refresh address counter receives the control signals produced from the refresh timer as its advance pulses, and forms refresh address signals

$\overline{ax}_0$ through $\overline{ax}_i$.

The operation of the multiplexer MPX is controlled by the control signal ϕ_{ref} . The multiplexer MPX selects the internal address signals $\overline{ax}_0$ through $\overline{ax}_i$ produced from the address buffer R-ADB when the control signal ϕ_{ref} is not produced, and selects the refresh address signals $\overline{ax}_0'$ through $\overline{ax}_i'$ when the control signal ϕ_{ref} is produced.

The timing control circuit TC generates various timing signals similar to those of the first embodiment in response to the row address strobe signal RAS, the column address strobe signal CAS, and the like that are supplied to the external terminals, in the same way as in the first embodiment. However, this embodiment is somewhat different from the first embodiment in that the internal circuit of the timing control circuit TC is constructed in such fashion as to respond to the refresh control signal

ϕ_{ref} . When the refresh control signal ϕ_{ref} is generated, the timing control signal TC controls the operations of the row system circuits, that is, the row address decoder R-DCR, the pre-charge circuit PC, the sense amplifier SA and the active restore circuit AR, shown in Fig. 1, in response to the refresh control signal.

According to this construction, the refresh operation is effected whenever the refresh control signal ϕ_{ref} is generated. In other words, when the refresh control signal ϕ_{ref} is generated, the refresh address signals $\overline{ax}_0$ through $\overline{ax}_i$ of the refresh address counter are supplied to the row address decoder R-DEC of Fig. 1 through the multiplexer MPX in response to the refresh control signal ϕ_{ref} . The control signal ϕ_{ref} actuates the timing control circuit TC, and the row system timing signals produced by the timing control circuit TC in turn actuate sequentially the pre-charge circuit PC, the row address decoder R-DCR, the sense amplifier SA and the active restore circuit AR of Fig. 1. As a result, the word line corresponding to the refresh address is selected, and the stored data of the memory cell coupled to the selected word line is refreshed.

The substrate bias voltage generation circuit V_{bb} -G and the level detection circuit VLD of this embodiment are substantially the same as those of Fig. 2.

In accordance with this embodiment, a logic synthesis circuit comprising of a CMOS gate circuit G_5 and CMOS inverter circuits IV_6 and IV_7 is provided so that the operation of the substrate bias voltage generation circuit V_{bb} -G is controlled by the refresh control signal ϕ_{ref} , too. The output of this logic synthesis circuit is set to the low level at the time of chip selection (a period in which the row address strobe signal RAS is at the low level) and at the time of the refresh operation.

The circuit portion of the intermittent operation inside the substrate bias voltage generation circuit V_{bb} -G is operated synchronously when the substrate leakage current is increased by the execution of the refresh operation, that is, when the timing control circuit TC and the row system circuits are operated by the refresh control signal ϕ_{ref} .

When battery back-up of a dynamic RAM is necessary, a power source device PS for forming a predetermined d.c. voltage from a commercial a.c. power source, for example, and a series circuit comprising of a battery E and a diode D are connected between the external terminal V_{cc} and GND. When the power source device PS is cut off, the power source voltage required by the RAM for holding the information or data is supplied from the battery E.

In the dynamic RAM of this embodiment, the refresh operation at the time of battery back-up is automatically executed without requiring any external control signals, in particular. Therefore, the RAM does not require the operations of other external devices at the time of battery back-up.

Since the lower power consumption by the substrate bias voltage generation circuit V_{bb} -G can be accomplished, the power consumption of the dynamic RAM of this embodiment can be reduced as a whole. Therefore, the battery life for battery back-up can be extended.

[Embodiment 3]

Fig. 5 is a circuit diagram showing a level detection circuit VLD and a substrate bias voltage generation circuit in accordance with still another embodiment of the invention.

The level detection circuit VLD comprises of a P-channel MOSFET Q_{26} , N-channel MOSFETs Q_{27} - Q_{29} and a CMOS inverter circuit IV_{10} as shown in the drawing. The substrate gate of the MOSFET Q_{26} is connected to the power terminal V_{cc} in the same way as in the foregoing embodiments. The substrate gates of the MOSFETs Q_{27} - Q_{29} consist of the P-type semiconductor substrate.

The detection output VD of the level detection circuit VLD is set to the high level substantially equal to the V_{cc} level or to the low level substantially equal to 0 V in accordance with the level of the back-bias voltage $-V_{bb}$ in the same way as in the foregoing embodiments.

The CMOS NAND gate circuit G_6 receives the detection output VD of the level detection circuit VLD and the control signal VCN_1 . The control signal VCN_1 is generated by an inverter circuit IV_7 shown in Fig. 4, for example. The output of the gate circuit G_6 is supplied to the substrate bias voltage generation circuit V_{bb} -G.

The substrate bias voltage generation circuit

V_{bb} -G comprises of the common oscillation circuit OSC, a CMOS inverter circuit IV_8 which act as a waveform shaping circuit, a CMOS NAND gate circuit G_7 , a CMOS inverter circuit IV_{11} , CMOS inverter circuits IV_9 and IV_{12} as a buffer amplifier, and rectification circuits CPC_1 and CPC_2 .

Since the output of the CMOS inverter circuit IV_8 is directly supplied to the input of the CMOS inverter circuit IV_9 , the latter generates steady pulse signals. In consequence, the rectification circuit CPC_1 is operated steadily.

The output of the CMOS inverter circuit IV_8 is supplied to the input of the CMOS inverter circuit IV_{12} through the gate circuit G_7 and the CMOS inverter circuit IV_{11} . Therefore, the output pulses of the CMOS inverter circuit IV_{12} are intermittent. The rectification circuit CPC_2 is therefore operated intermittently in accordance with the output of the inverter circuit IV_{12} .

The current supply capacity of the rectification circuit CPC_1 exhibiting the steady operation to the semiconductor substrate may be small in the same way as in the foregoing embodiments. Therefore, the charge pump capacitor C_3 may also be relatively small.

The charge pump capacitor in the rectification circuit CPC_2 , exhibiting the intermittent operation, is relatively large.

Though not particularly limited to this configuration, capacitors C_3 and C_4 are formed in an N-type region (not shown) that is in turn formed on the surface of the P-type semiconductor substrate, and have a construction similar to that of the P-channel MOSFET. The N-type well region in which these capacitors C_3 and C_4 are formed is held at the potential of the power terminal V_{cc} of the circuit, for example. This construction is somewhat advantageous for reducing the substrate leakage current.

In accordance with this embodiment, the oscillation circuit OSC is common to the rectification circuits CPC_1 and CPC_2 . As described already, the bias current supplied to the semiconductor substrate is associated with the operating frequency of the rectification circuit. The oscillation frequency of the oscillation circuit OSC is determined by the current supply capacity provided by the rectification circuit CPC_1 of the steady operation and by the current supply capacity provided by the rectification circuit CPC_2 of the intermittent operation. Therefore, the lower limit of the oscillation frequency of the oscillation circuit OSC is somewhat limited in comparison with that of the oscillation circuit OSC_2 of the steady operation shown in Fig. 2.

However, this embodiment does not include an oscillation circuit which consumes power during the operation of its own, such as the oscillation circuit

OSC_1 of the intermittent operation shown in Fig. 2.

Therefore, the number of necessary circuit elements can be reduced. Furthermore, the average power consumption of the RAM as a whole can be sufficiently reduced even when the power consumed by the common oscillation circuit OSC is somewhat greater than that of the oscillation circuit OSC_2 of Fig. 2, for example.

[Embodiment 4]

Fig. 6 is a circuit diagram of the substrate bias voltage generation circuit V_{bb} -G in accordance with still another embodiment of the present invention.

The substrate bias voltage generation circuit V_{bb} -G of this embodiment comprises of the oscillation circuit OSC, a CMOS inverter circuit IV_{13} which act as a waveform shaping circuit, a CMOS NAND gate circuit G_8 , CMOS inverter circuits IV_{14} and IV_{16} , CMOS inverter circuits IV_{15} and IV_{17} which act as buffer amplifier, charge pump capacitors C_5 and C_6 and N-channel MOSFETs Q_{35} through Q_{38} as rectification elements.

The circuit operation, when the control signal V_{CN2} formed in combination with the detection output of the level detection circuit and the control signal of the dynamic RAM as in the foregoing embodiment is at the low level, is as follows.

The outputs of the gate circuit G_8 and inverter circuit IV_{17} are at the high level irrespective of the output of the oscillation circuit OSC. The capacitor C_6 is under the charge state by the high level output of the inverter IV_{17} .

The output of the inverter IV_{15} is charged to the high and low levels in accordance with the output of the oscillation circuit OSC. Under this state, the rectification circuit comprising of the capacitor C_5 and the MOSFETs Q_{37} and Q_{38} is operated, and the back-bias voltage $-V_{bb}$ is supplied to the semiconductor substrate in response thereto. The MOSFET Q_{35} is kept substantially OFF because the maximum positive potential level appearing at the node N_1 is clamped by the MOSFET Q_{37} as the rectification element.

The circuit operation when the control signal V_{CN2} is at the high level is as follows.

When the output of the inverter circuit IV_{13} is raised to the high level in accordance with the output of the oscillation circuit OSC, the output of the inverter circuit IV_{15} is raised to the high level substantially equal to the power source voltage V_{cc} in response thereto, while the output of the inverter circuit IV_{17} is lowered to the low level substantially equal to 0 V. Since the capacitor C_6 is charged in advance, the node N_2 is set to the negative potential when the output of the inverter circuit IV_{17} is lowered to the low level. As the node N_2 is thus at the negative potential, the MOSFET Q_{35} as the

rectification element is rendered conductive. As a result, the negative potential formed by the capacitor C_5 is transmitted to the node N_1 through the MOSFET Q_{35} . The capacitor C_5 is charged by the high level produced from the inverter circuit IV_{15} and by the negative potential applied to the node N_1 to such a high level as to exceed the power source voltage V_{cc} . In other words, the capacitor C_5 is operated substantially as a bootstrap capacitor and the charging voltage of the capacitor C_5 is at the boost level.

Next, when the output of the inverter circuit IV_{13} is lowered to the low level, the output of the inverter circuit IV_{15} is lowered to the low level substantially equal to 0 V in response thereto. Since the capacitor C_5 is charged in advance to the boost level, the node N_1 is set to a large negative potential in response to the drop of the output of the inverter circuit IV_{15} to the low level. The potential of this node N_1 is supplied to the semiconductor substrate via the MOSFET Q_{35} . The output of the inverter circuit IV_{17} is raised to the high level substantially equal to the power source voltage in accordance with the low level output of the inverter circuit IV_{13} . The MOSFET Q_{36} is rendered conductive by the positive potential given to the node N_2 through the capacitor C_6 . As a result, the capacitor C_6 is charged again.

The operations described above are repeated in accordance with the change of the output of the inverter circuit IV_{13} . As a result, a large bias current is supplied to the semiconductor substrate within a period in which the control signal VCN_2 is at the high level.

In accordance with this embodiment, the two inverter circuits IV_{15} and IV_{17} having a relatively large driving capacity are operated so as to complement each other so that the transient current flowing through the power source wiring inside the RAM can be reduced, and noise in the power source wiring can be therefore reduced.

[Effects]

(1) The operations of the oscillation circuit for forming the back-bias voltage and its rectification circuit are selectively stopped by monitoring the level of the back-bias voltage, so that the consumption of substantially wasted current can be restricted. As a result, the lower power consumption of a semiconductor integrated circuit device with a built-in substrate back-bias voltage generation circuit can be accomplished.

(2) The present invention disposes the substrate back-bias voltage generation circuit having only such a small current supply capacity that compensates for a leakage current at the time of non-selection, and another substrate back-bias

voltage generation circuit which is selectively operated by the level monitor output of the substrate back-bias voltage. In addition, the invention makes invalid the monitor output when the internal circuits are operated. According to this arrangement, a substrate back-bias voltage which is at a substantially constant level can be formed with reduced power consumption.

(3) Due to the effects (1) and (2), the power consumption of the substrate bias voltage generation circuit can be reduced, so that the service life of a battery at the time of the battery back-up operation can be extended.

(4) A level limiter operation by the P-channel MOSFETs to the gates of which the ground potential of the circuit is supplied and the N-channel MOSFETs in the diode form can detect the level of a negative voltage with respect to the ground potential as the reference by using substantially the positive power source voltage V_{cc} alone, with a simple circuit construction.

Though the invention has thus been described definitely with reference to some preferred embodiments thereof, the invention is not particularly limited thereto, but can of course be modified or changed in various manners without departing from the gist thereof. For example, in those semiconductor integrated circuit devices which are made operative by chip selection signals such as in RAMs, the monitor output of the substrate back-bias voltage may be made invalid by the chip selection signal in place of the internal control signal RAS_1 in the circuit of the embodiment shown in Fig. 2. The oscillation circuit which is operated steadily by turning on the power source voltage and its rectification circuit are not essentially necessary.

The circuit construction in which the substrate bias generation circuit is divided into the circuit portion exhibiting the steady operation and the circuit portion exhibiting the intermittent operation is desirable from the aspect of the prevention of the unnecessary increase of the sizes of the circuit elements forming the circuit portion exhibiting the intermittent operation. If necessary, however, the circuit having a small current supply capacity and the circuit having a large current supply capacity may be operated selectively. A plurality of circuit portions exhibiting the intermittent operation may be disposed and may be controlled individually.

In the present invention, the term "substrate" of the "substrate bias generation circuit" means one semiconductor region such as the substrate gate of a field effect element but is not intended to mean only a semiconductor substrate. For example, if a memory cell is formed in a P-type well region formed on the surface of an N-type semiconductor substrate in order to reduce the soft error of the memory resulting from α rays and the

back-bias voltage is applied to the P-type well region, the term "substrate" means that P-type well region.

In addition to the use of the dummy cells, the reference voltage for reading out the memory cells constituting the dynamic RAM may be formed by short-circuiting the complementary data lines that are at the high and low levels under the high impedance state, without using the dummy cells. The reference voltage in this case is at the intermediate level. Various other circuit constructions may further be employed. For example, peripheral circuits such as the address buffers, the address decoders, and the like may be constituted by CMOS static circuits. The X and Y address signals may be supplied from mutually independent external terminals and a detection circuit for detecting the change timing of the address signal is disposed in order to generate various timing signals necessary for the operations of the internal circuits.

Besides the semiconductor memories such as the dynamic RAMs and the static RAMs described above, the present invention can be applied widely to semiconductor integrated circuit devices equipped with a built-in substrate bias generation circuit.

Claims

1. A semiconductor integrated circuit device comprising:
 - a first circuit which includes insulated gate field effect transistors (Qm) having a common substrate region to which a back-bias voltage (-Vbb) is supplied, the operation of said first circuit being controlled by a control signal (RAST), and
 - a circuit (Vbb-G) for generating said back-bias voltage (-Vbb), the current output capacity of said back-bias voltage generation circuit (Vbb-G) being changed on the basis of said control signal (RAST) during the period in which said first circuit is operative, characterized in
 - that a level detection circuit (VLD) for detecting the level of said back-bias voltage (-Vbb) is provided, wherein said current output capacity is changed also on the basis of the detection signal of said level detection circuit (VLD), and
 - that said back-bias voltage generation circuit (Vbb-G) comprises a first rectification circuit delivering said back-bias voltage and including a capacitor (C1) and a plurality of rectification elements (Q18, Q19), and a control circuit (G1) for controlling pulse signals supplied to said first rectification circuit in response to the output signal of said level detection circuit (VLD) and said control signal (RAST).
2. The device of claim 1 wherein said back-bias voltage generation circuit (Vbb-G) comprises a second rectification circuit including a capacitor (C2) and a plurality of rectification elements (Q20, Q21) and receiving periodic pulse signals.
3. The device of claim 2 wherein said pulse signal to be supplied to said first rectification circuit is set to a level such that said capacitor (C1) of said first rectification circuit is brought into a pre-charge state when said control signal (RAST) is at such a level as to render said first circuit inoperative.
4. The device of claim 2 or 3 wherein said back-bias voltage generation circuit (Vbb-G) comprises a first oscillation circuit (OSC2) for generating pulse signals to be supplied to said second rectification circuit and a second oscillation circuit (OSC1) having the operation thereof controlled in response to an operation control signal produced from said control circuit (G1), and generating pulse signals to be supplied to said first rectification circuit.
5. The device of claim 4 wherein said second oscillation circuit (OSC1) comprises a ring oscillator forming a feed-back loop on the basis of said control signal (RAST).
6. The device of claim 4 or 5, wherein said control circuit (G1) generates said operation control signal for making said second oscillation circuit (OSC1) operative on the basis of said operation control signal during the period in which said first circuit is operative and during the period in which said detection signal is generated.
7. The device of claim 6 wherein said level detection circuit (VLD) comprises a level shift circuit (Q10 ... Q14) for generating a level-shifted output voltage with respect to said back-bias voltage (-Vbb) upon receiving said back-bias voltage, and a level discrimination circuit (Q15 ... Q17, IVo) receiving the output of said level shift circuit.
8. The device of claim 7 wherein said level shift circuit comprises a plurality of level shift elements (Q12 ... Q14) each including an insulated gate field effect transistor of diode connection, that are connected in series with one another, and a bias element (Q10, Q11).



back-bias voltage is applied to the P-type well region, the term "substrate" means that P-type well region.

In addition to the use of the dummy cells, the reference voltage for reading out the memory cells constituting the dynamic RAM may be formed by short-circuiting the complementary data lines that are at the high and low levels under the high impedance state, without using the dummy cells. The reference voltage in this case is at the intermediate level. Various other circuit constructions may further be employed. For example, peripheral circuits such as the address buffers, the address decoders, and the like may be constituted by CMOS static circuits. The X and Y address signals may be supplied from mutually independent external terminals and a detection circuit for detecting the change timing of the address signal is disposed in order to generate various timing signals necessary for the operations of the internal circuits.

Besides the semiconductor memories such as the dynamic RAMs and the static RAMs described above, the present invention can be applied widely to semiconductor integrated circuit devices equipped with a built-in substrate bias generation circuit.

Claims

1. A semiconductor integrated circuit device comprising:
 - a first circuit which includes insulated gate field effect transistors (Qm) having a common substrate region to which a back-bias voltage (-Vbb) is supplied, the operation of said first circuit being controlled by a control signal (RAST), and
 - a circuit (Vbb-G) for generating said back-bias voltage (-Vbb), the current output capacity of said back-bias voltage generation circuit (Vbb-G) being changed on the basis of said control signal (RAST) during the period in which said first circuit is operative, characterized in
 - that a level detection circuit (VLD) for detecting the level of said back-bias voltage (-Vbb) is provided, wherein said current output capacity is changed also on the basis of the detection signal of said level detection circuit (VLD), and
 - that said back-bias voltage generation circuit (Vbb-G) comprises a first rectification circuit delivering said back-bias voltage and including a capacitor (C1) and a plurality of rectification elements (Q18, Q19), and a control circuit (G1) for controlling pulse signals supplied to said first rectification circuit in response to the output signal of said level detection circuit (VLD) and said control signal (RAST).
2. The device of claim 1 wherein said back-bias voltage generation circuit (Vbb-G) comprises a second rectification circuit including a capacitor (C2) and a plurality of rectification elements (Q20, Q21) and receiving periodic pulse signals.
3. The device of claim 2 wherein said pulse signal to be supplied to said first rectification circuit is set to a level such that said capacitor (C1) of said first rectification circuit is brought into a pre-charge state when said control signal (RAST) is at such a level as to render said first circuit inoperative.
4. The device of claim 2 or 3 wherein said back-bias voltage generation circuit (Vbb-G) comprises a first oscillation circuit (OSC2) for generating pulse signals to be supplied to said second rectification circuit and a second oscillation circuit (OSC1) having the operation thereof controlled in response to an operation control signal produced from said control circuit (G1), and generating pulse signals to be supplied to said first rectification circuit.
5. The device of claim 4 wherein said second oscillation circuit (OSC1) comprises a ring oscillator forming a feed-back loop on the basis of said control signal (RAST).
6. The device of claim 4 or 5, wherein said control circuit (G1) generates said operation control signal for making said second oscillation circuit (OSC1) operative on the basis of said operation control signal during the period in which said first circuit is operative and during the period in which said detection signal is generated.
7. The device of claim 6 wherein said level detection circuit (VLD) comprises a level shift circuit (Q10 ... Q14) for generating a level-shifted output voltage with respect to said back-bias voltage (-Vbb) upon receiving said back-bias voltage, and a level discrimination circuit (Q15 ... Q17, IV0) receiving the output of said level shift circuit.
8. The device of claim 7 wherein said level shift circuit comprises a plurality of level shift elements (Q12 ... Q14) each including an insulated gate field effect transistor of diode connection, that are connected in series with one another, and a bias element (Q10, Q11).



The device of claim 7 or 8 wherein said level discrimination circuit comprises a hysteresis circuit (Q15 ... Q17, IV0).

10. The device of any of claims 4 to 9 wherein the oscillation frequency of said first oscillation circuit (OSC2) is lower than that of said second oscillation circuit (OSC1).

11. The device of any of claims 1 to 4 wherein said first circuit comprises a memory (MARY) whose operation is controlled by said control signal (RAST).

12. The device of claim 11' wherein said memory (MARY) comprises a dynamic type random access memory, and said control signal (RAST) is a chip selection signal (RAST).

13. The device of claim 12 wherein said dynamic type random access memory (MARY) is rendered operative at the time of chip selection determined by said chip selection signal (RAST) and at the time of a refresh operation determined by a refresh control signal (ϕ_{ref}), and said control circuit (G1) generates said operation control signal for making said second oscillation circuit (OSC1) operative in synchronism with the operative state of said dynamic type random access memory, on the basis of said chip selection signal (RAST) and said refresh control signal (ϕ_{ref}).

14. The device of claim 13, wherein said control circuit (G1) generates said operation control signal for making said second oscillation circuit (OSC1) operative during the period in which said dynamic type random access memory (MARY) is made operative on the basis of said chip selection signal (RAST) and said refresh control signal (ϕ_{ref}), and during the period in which the detection signal is generated from said level detection circuit (VLD).

15. The device of claim 2 wherein said back-bias generation circuit (Vbb-G) comprises a common oscillation circuit (OSC) generating pulse signals to be supplied to said first and second rectification circuits (CPC2, CPC1), said control circuit and said first and second rectification circuits, and wherein said control circuit includes a gate circuit (G7) inhibiting the operation of said first rectification circuit (CPC2) when said first circuit is made inoperative.

16. The device of claim 15 wherein said gate circuit (G7) is disposed between the output terminal of said oscillation circuit (OSC) and the

input terminal of said first rectification circuit (CPC2), and the operation of said gate circuit (G7) is controlled by said control signal.

17. The device of claim 15 or 16, wherein said gate circuit (G7) inhibits the operation of said first rectification circuit (CPC2) when said first circuit is made inoperative and when the detection signal (VD) is not generated from said level detection circuit (VLD).

18. The device of claim 17 wherein said level detection circuit (VLD) comprises a level shift circuit (Q26 ... Q29) generating an output voltage level-shifted with respect to said back-bias voltage (-Vbb) upon receiving said back-bias voltage, and a level discrimination circuit (IV10) receiving the output of said level shift circuit.

19. The device of claim 18 wherein said level shift circuit comprises a plurality of level shift elements (Q27 ... Q29) each of which includes an insulated gate field effect transistor which transistors are connected in series with one another, and a bias element (Q26) applying a bias current to said level shift elements.

20. The device of claim 2, wherein said back-bias voltage generation circuit (Vbb-G) comprises said first rectification circuit (C6, Q35, Q36) including a first capacitor (C6) which increases the pre-charge level of a second capacitor (C5) when said first rectification circuit is made operative in response to said control signal (VCN2) supplied to a gate circuit (G8); and said second rectification circuit (C5, Q37, Q38) including said second capacitor (C5) which is pre-charged in response to a first level of a periodic pulse signal and which applies a bias potential to said common substrate region to a first node (N1) in response to a second level of said pulse signal, a first switch circuit (Q37) connected to said first node (N1) and forming a pre-charged path for said second capacitor (C5), and a second switch circuit (Q38) disposed between said first node (N1) and said common substrate region and caused to operate substantially complementarily with respect to said first switch circuit (Q37).

Patentansprüche

1. Integrierte Halbleiterschaltungsanordnung, umfassend
eine erste Schaltung mit Isolierschicht-Feldeffekttransistoren (Qm) mit einem gemein-



samen Substratbereich, an dem eine Substratvorspannung (-Vbb) liegt, wobei der Betrieb der ersten Schaltung durch ein Steuersignal (RAST) gesteuert wird, und

eine Schaltung (Vbb-G) zur Erzeugung der Substratvorspannung (-Vbb), wobei die Stromausgangskapazität der diese Vorspannung erzeugenden Schaltung (Vbb-G) während der Periode, in der die erste Schaltung in Betrieb ist, aufgrund des Steuersignals (RAST) geändert wird,

dadurch gekennzeichnet,

daß eine Pegeldetektorschaltung (VLD) zur Erfassung des Pegels der Substratvorspannung (-Vbb) vorgesehen ist, wobei die Stromausgangskapazität auch aufgrund des Erfassungssignals der Pegeldetektorschaltung (VLD) geändert wird, und

daß die die Substratvorspannung erzeugende Schaltung (Vbb-G) eine diese Vorspannung abgebende erste Gleichrichterstufe mit einem Kondensator (C1) und mehreren Gleichrichterelementen (Q18, Q19) sowie eine Steuerschaltung (G1) zur Steuerung von Impulssignalen umfaßt, die in Abhängigkeit vom Ausgangssignal der Pegeldetektorschaltung (VLD) und vom Steuersignal (RAST) der ersten Gleichrichterstufe zugeführt werden.

2. Anordnung nach Anspruch 1, wobei die die Substratvorspannung erzeugende Schaltung (Vbb-G) eine periodische Impulssignale empfangende zweite Gleichrichterstufe mit einem Kondensator (C2) und mehreren Gleichrichterelementen (Q20, Q21) umfaßt.
3. Anordnung nach Anspruch 2, wobei das der ersten Gleichrichterstufe zuzuführende Impulssignal auf einen derartigen Pegel gelegt ist, daß der Kondensator (C1) der ersten Gleichrichterstufe in einen Voraufgeladenzustand gelangt, wenn das Steuersignal (RAST) sich auf einem derartigen Pegel befindet, daß die erste Schaltung nicht in Betrieb ist.
4. Anordnung nach Anspruch 2 oder 3, wobei die die Substratvorspannung erzeugende Schaltung (Vbb-G) eine erste Oszillatorschaltung (OSC2) zur Erzeugung von der zweiten Gleichrichterstufe zuzuführenden Impulssignalen und eine zweite Oszillatorschaltung (OSC1) umfaßt, deren Betrieb in Abhängigkeit von einem von der Steuerschaltung (G1) erzeugten Steuersignal gesteuert ist und die Impulssignale zur Zuführung an die erste Gleichrichterstufe erzeugt.
5. Anordnung nach Anspruch 4, wobei die zweite

Oszillatorschaltung (OSC1) einen Ringoszillator umfaßt, der aufgrund des Steuersignals (RAST) eine Rückkopplungsschleife bildet.

6. Anordnung nach Anspruch 4 oder 5, wobei die Steuerschaltung (G1) das Betriebssteuersignal erzeugt, um aufgrund dessen während der Periode, in der die erste Schaltung in Betrieb ist, sowie während der Periode, in der das Erfassungssignal erzeugt wird, die zweite Oszillatorstufe (OSC1) in Betrieb zu setzen.
7. Anordnung nach Anspruch 6, wobei die Pegeldetektorschaltung (VLD) eine Pegelschiebestufe (Q10...Q14), die bei Empfang der Substratvorspannung (-Vbb) eine bezüglich derselben im Pegel verschobene Ausgangsspannung erzeugt, sowie eine Pegeldiskriminatorstufe (Q15...Q17, IV0) umfaßt, die das Ausgangssignal der Pegelschiebestufe empfängt.
8. Anordnung nach Anspruch 7, wobei die Pegelschiebestufe mehrere Pegelschiebeelemente (Q12...Q14), deren jedes einen Isolierschicht-Feldeffekttransistor in Diodenschaltung aufweist, wobei diese Transistoren in Serie liegen, sowie ein Vorspannungselement (Q10, Q11) umfaßt.
9. Anordnung nach Anspruch 7 oder 8, wobei die Pegeldiskriminatorstufe eine Hystereseschaltung (Q15...Q17, IV0) umfaßt.
10. Anordnung nach einem der Ansprüche 4 bis 9, wobei die Oszillatorfrequenz der ersten Oszillatorschaltung (OSC2) niedriger ist als die der zweiten Oszillatorschaltung (OSC1).
11. Anordnung nach einem der Ansprüche 1 bis 4, wobei die erste Schaltung einen Speicher (MARY) aufweist, dessen Betrieb von dem Steuersignal (RAST) gesteuert ist.
12. Anordnung nach Anspruch 11, wobei der Speicher (MARY) einen dynamischen Random-Access-Speicher umfaßt und das Steuersignal (RAST) ein Chip-Auswahlsignal (RAST) ist.
13. Anordnung nach Anspruch 12, wobei der dynamische Random-Access-Speicher (MARY) zu dem durch das Chip-Auswahlsignal (RAST) bestimmten Zeitpunkt der Chipauswahl sowie zu dem von einem Auffrisch-Steuersignal (ϕ_{ref}) bestimmten Zeitpunkt eines Auffrischvorgangs in Betrieb gesetzt wird, und wobei die Steuerschaltung (G1) das Betriebssteuersignal, das die zweite Oszillatorschaltung (OSC1) in Betrieb setzt, aufgrund des Chip-Auswahlsignals



(RAST) und des Auffrisch-Steuersignals (ϕ_{ref}) synchron mit dem Betriebszustand des dynamischen Random-Access-Speichers erzeugt.

14. Anordnung nach Anspruch 13, wobei die Steuerschaltung (G1) das Betriebssteuersignal erzeugt, um die zweite Oszillatorschaltung (OSC1) während der Periode, in der der dynamische Random-Access-Speicher (MARY) aufgrund des Chip-Auswahlsignals (RAST) und des Auffrisch-Steuersignals (ϕ_{ref}) in Betrieb ist, sowie während der Periode, in der das Erfassungssignal von der Pegeldetektorschaltung (VLD) erzeugt wird, in Betrieb zu setzen.

15. Anordnung nach Anspruch 2, wobei die die Substratvorspannung erzeugende Schaltung (Vbb-G) eine gemeinsame Oszillatorschaltung (OSC) zur Erzeugung von der ersten und der zweiten Gleichrichterstufe (CPC2, CPC1) zuzuführenden Impulssignalen, die Steuerschaltung und die ersten und die zweite Gleichrichterstufe umfaßt, und wobei die Steuerschaltung eine Torschaltung (G7) aufweist, die den Betrieb der ersten Gleichrichterstufe (CPC2) inhibiert, wenn die erste Schaltung außer Betrieb ist.

16. Anordnung nach Anspruch 15, wobei die Torschaltung (G7) zwischen der Ausgangsklemme der Oszillatorschaltung (OSC) und der Eingangsklemme der ersten Gleichrichterstufe (CPC2) angeordnet ist und ihr Betrieb von dem Steuersignal gesteuert wird.

17. Anordnung nach Anspruch 15 oder 16, wobei die Torschaltung (G7) den Betrieb der ersten Gleichrichterstufe (CPC2) inhibiert, wenn die erste Schaltung außer Betrieb ist und wenn von der Pegeldetektorschaltung (VLD) das Erfassungssignal (GD) nicht erzeugt wird.

18. Anordnung nach Anspruch 17, wobei die Pegeldetektorschaltung (VLD) eine Pegelschiebestufe (Q26...Q29), die bei Empfang der Substratvorspannung (-Vbb) eine bezüglich derselben im Pegel verschobene Ausgangsspannung erzeugt, sowie eine Pegeldiskriminatorstufe (IV10) aufweist, die das Ausgangssignal der Pegelschiebestufe empfängt.

19. Anordnung nach Anspruch 18, wobei die Pegelschiebestufe mehrere Pegelschiebeelemente (Q27...Q29), deren jedes einen Isolierschicht-Feldeffekttransistor aufweist, wobei diese Transistoren in Serie liegen, sowie ein Vorspannungselement (Q26) umfaßt, das die Pegelschiebeelemente mit einem Vorstrom versorgt.

20. Anordnung nach Anspruch 2, wobei die die Substratvorspannung erzeugende Schaltung (Vbb-G) umfaßt:

eine erste Gleichrichterstufe (C6, Q35, Q36) mit einem ersten Kondensator (C6), der den Voraufladepegel eines zweiten Kondensators (C5) erhöht, wenn die erste Gleichrichterstufe aufgrund des einer Torschaltung (G8) zugeführten Steuersignals (VCN2) in Betrieb gesetzt wird, und

eine zweite Gleichrichterstufe (C5, Q37, Q38), die den zweiten Kondensator (C5), der in Abhängigkeit von einem ersten Pegel eines periodischen Impulssignales voraufgeladen wird und in Abhängigkeit von einem zweiten Pegel dieses Impulssignals dem gemeinsamen Substratbereich an einem ersten Knotenpunkt (N1) ein Vorspannpotential zuführt, eine erste Schaltstufe (Q37), die mit dem ersten Knotenpunkt (N1) verbunden ist und einen Voraufladepfad für den zweiten Kondensator (C5) bildet, sowie eine zweite Schaltstufe (Q38) umfaßt, die zwischen dem ersten Knotenpunkt (N1) und dem gemeinsamen Substratbereich angeordnet ist und im wesentlichen komplementär zu der ersten Schaltstufe (Q37) arbeitet.

Revendications

1. Dispositif à circuits intégrés à semiconducteurs comprenant :

un premier circuit qui comprend des transistors à effet de champ à grille isolée (Qm) possédant une région de substrat commune, à laquelle une tension de polarisation arrière (-Vbb) est appliquée, le fonctionnement dudit premier circuit étant commandé par un signal de commande (RAST), et

un circuit (Vbb-G) pour produire une tension de polarisation arrière (-Vbb), la capacité de délivrance de courant dudit circuit (Vbb-G) de production de la tension de polarisation arrière étant modifiée sur la base dudit signal de commande (RAST) pendant la période pendant laquelle ledit premier circuit fonctionne,

caractérisé en ce

qu'il est prévu un circuit de détection de niveau (VLD) pour détecter le niveau de ladite tension de polarisation arrière (-Vbb), ladite capacité de sortie de courant étant également modifiée sur la base du signal de détection dudit circuit de détection de niveau (VLD), et

que ledit circuit (Vbb-G) de production de la tension de polarisation arrière comprend un premier circuit redresseur délivrant ladite tension de polarisation arrière et comprenant un condensateur (C1) et une pluralité d'éléments



- redresseurs (Q18,Q19) et un circuit de commande (G1) pour commander des signaux impulsionsnels envoyés audit premier circuit redresseur en réponse audit signal de sortie dudit circuit de détection de niveau (VLD) et audit signal de commande (RAST).
2. Dispositif selon la revendication 1, dans lequel ledit circuit (Vbb-G) de production de la tension de polarisation arrière comprend un second circuit redresseur comprenant un condensateur (C2) et une pluralité d'éléments redresseurs (Q20,Q21) et recevant des signaux impulsionsnels périodiques.
 3. Dispositif selon la revendication 2, dans lequel ledit signal impulsionsnel devant être envoyé audit premier circuit redresseur est réglé à un niveau tel que ledit condensateur (C1) dudit premier circuit redresseur est placé dans un état de précharge lorsque ledit signal de commande (RAST) est à un niveau tel qu'il rend inactif le premier circuit.
 4. Dispositif selon la revendication 2 ou 3, dans lequel ledit circuit (Vbb-G) de production de la tension de polarisation arrière comprend un premier circuit oscillateur (OSC2) pour produire des signaux impulsionsnels devant être envoyés audit second circuit redresseur et un second circuit oscillateur (OSC1) dont le fonctionnement est commandé en réponse à un signal de fonctionnement produit par ledit circuit de commande (G1), et produisant des signaux impulsionsnels devant être envoyés audit premier circuit redresseur.
 5. Dispositif selon la revendication 4, dans lequel ledit second circuit oscillateur (OSC1) comprend un oscillateur en anneau formant une boucle de réaction sur la base dudit signal de commande (RAST).
 6. Dispositif selon la revendication 4 ou 5, dans lequel ledit circuit de commande (G1) produit ledit signal de commande de fonctionnement pour rendre ledit second circuit oscillateur (OSC1) actif sur la base dudit signal de commande de fonctionnement pendant la période pendant laquelle ledit premier circuit est actif et pendant la période pendant laquelle ledit signal de détection est produit.
 7. Dispositif selon la revendication 6, dans lequel ledit circuit de détection de niveau (VLD) comprend un circuit de décalage de niveau (Q10...Q14) pour produire une tension de sortie à niveau décalé par rapport à ladite tension de polarisation arrière (-Vbb) lors de la réception de ladite tension de polarisation arrière, et un circuit discriminateur de niveau (Q4...Q17, IV0) recevant le signal de sortie dudit circuit de décalage de niveau.
 8. Dispositif selon la revendication 7, dans lequel ledit circuit de décalage de niveau comprend une pluralité d'éléments de décalage de niveau (Q12...Q14) comprenant chacun un transistor à effet de champ à grille isolée, branché en diode, ces transistors étant branchés en série, et un élément de polarisation (Q10,Q11).
 9. Dispositif selon la revendication 7 ou 8, dans lequel ledit circuit discriminateur de niveau comprend un circuit à hystérésis (Q15...Q17, IV0).
 10. Dispositif selon l'une quelconque des revendications 4 à 9, dans lequel la fréquence d'oscillations dudit premier circuit oscillateur (OSC2) est inférieure à celle dudit second circuit oscillateur (OSC1).
 11. Dispositif selon l'une quelconque des revendications 1 à 4, dans lequel ledit premier circuit comprend une mémoire (MARY), dont le fonctionnement est commandé par ledit signal de commande (RAST).
 12. Dispositif selon la revendication 11, dans lequel ladite mémoire (MARY) comprend une mémoire à accès direct de type dynamique, et ledit signal de commande (RAST) est un signal de sélection de microplaquette (RAST).
 13. Dispositif selon la revendication 12, dans lequel ladite mémoire à accès direct de type dynamique (MARY) est rendue active au moment de la sélection de microplaquette déterminée par ledit signal de sélection de microplaquette (RAST) et au moment d'une opération de régénération déterminée par un signal de commande de régénération (ϕ_{ref}), et ledit circuit de commande (G1) produit ledit signal de commande de fonctionnement pour rendre actif ledit second circuit oscillateur (OSC1) en synchronisme avec l'état de fonctionnement de ladite mémoire à accès direct de type dynamique, sur la base dudit signal de sélection de microplaquette (RAST) et dudit signal de commande de régénération (ϕ_{ref}).
 14. Dispositif selon la revendication 13, dans lequel ledit circuit de commande (G1) produit ledit signal de commande de fonctionnement pour rendre actif ledit second circuit oscillateur



(OSC1) pendant la période pendant laquelle ladite mémoire à accès direct de type dynamique (MARY) est rendue active sur la base dudit signal de sélection de microplaquette (FAST) et dudit signal de commande de régénération (ϕ_{ref}), et pendant la période pendant laquelle le signal de détection est produit par ledit circuit de détection de niveau (VLD).

15. Dispositif selon la revendication 2, dans lequel ledit circuit (Vbb-G) de production de la tension de polarisation comprend un circuit oscillateur commun (OSC) produisant des signaux impulsionnels devant être envoyés auxdits premier et second circuits redresseurs (CPC2, CPC1), auxdits circuits de commande et auxdits premier et second circuits redresseurs, et dans lequel ledit circuit de commande comprend un circuit de porte (G7) empêchant le fonctionnement dudit premier circuit redresseur (CPC2) lorsque ledit premier circuit est rendu actif.

16. Dispositif selon la revendication 15, dans lequel ledit circuit de porte (G7) est disposé entre la borne de sortie dudit circuit oscillateur (OSC) et la borne d'entrée dudit premier circuit redresseur (CPC2), et le fonctionnement dudit circuit de porte (G7) est commandé par ledit signal de commande.

17. Dispositif selon la revendication 15 ou 16, dans lequel ledit circuit de porte (G7) empêche le fonctionnement dudit premier circuit redresseur (CPC2) lorsque ledit premier circuit est rendu actif et lorsque le signal de détection (VD) n'est pas produit par ledit circuit de détection de niveau (VLD).

18. Dispositif selon la revendication 17, dans lequel ledit circuit de détection de niveau (VLD) comprend un circuit de décalage de niveau (Q26...Q29) produisant une tension de sortie dont le niveau est décalé par rapport à ladite tension de polarisation arrière (-Vbb) lors de la réception de ladite tension de polarisation arrière, et un circuit discriminateur de niveau (IV10) recevant le signal de sortie dudit circuit de décalage de niveau.

19. Dispositif selon la revendication 18, dans lequel ledit circuit de décalage de niveau comprend une pluralité d'éléments de décalage de niveau (Q27...Q29), dont chacun comprend un transistor à effet de champ à grille isolée, ces transistors étant branchés en série entre eux, et un élément de polarisation (Q26) appliquant un courant de polarisation audit élément de

décalage de niveau.

20. Dispositif selon la revendication 2, dans lequel ledit circuit (Vbb-G) de production de la tension de polarisation arrière comprend

ledit premier circuit redresseur (C6, Q35, Q36) comprenant un premier condensateur (C6) qui augmente le niveau de précharge d'un second condensateur (C5) lorsque ledit premier circuit redresseur est rendu actif en réponse audit signal de commande (VCN2) envoyé à un circuit de porte (G8);

ledit second circuit redresseur (C5, Q37, Q38) comprenant ledit second condensateur (C5) qui est préchargé en réponse à un premier niveau d'un signal impulsionnel périodique et qui applique un potentiel de polarisation à ladite région de substrat commune, en un premier noeud (N1) en réponse à un second niveau dudit signal impulsionnel, un premier circuit de commutation (Q36) raccordé audit premier noeud (N1) et formant un trajet préchargé pour ledit second condensateur (C5), et un second circuit de commutation (Q38) disposé entre ledit premier noeud (N1) et ladite région de substrat commune et tenu de fonctionner d'une manière sensiblement complémentaire par rapport audit premier circuit de commutation (Q37).