

Description

The invention relates to a mixer arrangement comprising first and second mixer stages to which quadrature mixing signals are applied from an oscillator circuit, these two mixer stages being coupled to a super-position circuit.

Such a mixer arrangement is disclosed in the article "A third method of generation and detection of SSB-signals" by D. K. Weaver, published in Proceedings of the IRE, 1956, Vol. 44, No. 12, pages 1703—1705.

In some applications of the prior art mixer arrangements, the frequency of the oscillator is located in the frequency range of the desired signal at the outputs of the two mixer stages, such as, for example, in single-sideband receivers based on the demodulation principle described in the above-mentioned article. In those cases this desired signal can be seriously disturbed by parasitic oscillator cross-talk and/or d.c. off-set in this mixer stages. A suppression of these oscillator frequency-coupled interferences, called oscillator interference hereinafter for the sake of brevity in the desired signal by means of notch filters results, especially in the above-described application of the mixer arrangement, in a signal component suppression which is audible to an annoying degree.

A feed forward compensation of the oscillator interference by means of a compensating signal derived from the oscillator signal, such as, for example, described in United Kingdom Patent Application No. 811 274 to compensate for oscillator radiation, only operates correctly for one given amplitude and phase of the oscillator interference. However, the amplitude and the phase of the oscillator interference vary and depend *inter alia* on the oscillator frequency and on the magnitude of said de-offset of the relevant mixer stages and on the magnitude of the reactance of the undesired parasitic, usually capacitive couplings in or at the mixer stages, which can be influenced to such an extent by constructional tolerances, temperature fluctuations, ageing etc. that they can in practice not be determined unambiguously.

The invention has for its object to provide a mixer arrangement of the type described in the opening paragraph in which interferences coupled to the oscillator frequency and being a result of oscillator cross-talk and/or de-offset in the mixer stages can be suppressed to a significant extent, adaptively and substantially independent of the variation of their phase and amplitude, without affecting adjacent signal components.

According to the invention, such a mixer arrangement is characterized by first and second quadrature interference negative feedback paths for a negative feedback of oscillator frequency-coupled interferences from an output of the superposition circuit to inputs of two mixer stages, comprising first and second synchronous detectors, respectively coupled to the output of

the superposition circuit and also *via* first and second low-pass filters to inputs of the first and second mixer stages, quadrature carriers which are in an in-phase or an anti-phase relationship with the quadrature mixing signals being applied to these synchronous detectors from the oscillator circuit, whereas for the case in which there is an in-phase relationship between at least one of the said carriers and one of the said mixing signals the interference negative feedback path in which the synchronous detector which is fed by the last-mentioned carrier is included also comprises an inverter circuit for inverting the sign of the signal.

The invention is based on the recognition that the total resultant oscillator interference at the output of the superposition circuit can be resolved into quadrature noise components in the respective phase directions of the quadrature mixing signals applied to the two mixer stages and that the said quadrature noise components can be suppressed in a simple way by negatively feeding them back to the input of the respective mixer stages after a frequency translation.

When the measure according to the invention is applied, the magnitude of the said quadrature noise components is measured, or in other words converted into varying d.c. voltages by means of the two synchronous detectors and the two low-pass filters and a negative feedback of the interference is effected by applying these d.c. voltages with inverted signs to the two mixer stages. Therein these varying d.c. voltages modulate the said quadrature mixing signals, which results in quadrature noise compensating signals which in the superposition circuit suppress to a significant extent said total resultant oscillator interference at an adequate negative feedback gain.

The signal inversion of the signal in each of the two quadrature interference negative feedback paths can be obtained in different manners, for example by bringing the carrier or carriers required for the synchronous detection of one or both of the said quadrature noise components in anti-phase relationship with the mixing signal or mixing signals required for the modulation thereof, which can, for example, be realised in a simple way with a push-pull construction of the oscillator circuit. If, because of a given construction of the oscillator circuit one can only dispose of quadrature carriers, which are inphase with the quadrature mixing signals then a sign inversion is obtained by means of said inverter circuit, which may be included in the RF-section (for the synchronous detector) or in the LF section (subsequent to the synchronous detector) of the relevant interference negative feedback path.

A preferred embodiment of a mixer arrangement is characterized by an in-phase relationship between the two carriers and the two mixing signals, by first and second subtracting circuits whose inverting inputs are coupled to the first and second low-pass filters, respectively, whose non-inverting inputs are coupled to first and

second quadrature inputs of the mixer arrangement, respectively and whose outputs are coupled to the inputs of the first and the second mixing stages, respectively and in that the output of the superposition circuit is connected to an output of the mixer arrangement.

When this measure is applied, the mixer arrangement is particularly suitable for use in receivers based on the demodulation principle as described, for example, in the above-mentioned article. The mixer arrangement is then preceded by an RF-tuning arrangement comprising a pair of quadrature mixer stages in which a desired RF-receiving signal is converted into a pair of low-frequency quadrature signals, at which a folding of the frequency spectrum may occur. Depending on the choice of the oscillator frequency, these low-frequency quadrature signals are converted in the mixer arrangement in a manner which is known *per se* into a baseband or intermediate-frequency signals. To that end, said two mixer stages of the mixer arrangement have two functions: on the one hand they form the above-mentioned modulated quadrature compensating signals, on the other hand they have a signal processing function.

Another preferred embodiment of the mixer arrangement, is characterized by a further mixing signal is applied from the oscillator circuit, an input of the mixer arrangement corresponding to an input of the third mixer stage and an output of the third mixer stage being connected to an input of the superposition circuit.

When this measure is applied, the further mixer stage has for its sole object to process the signal and the first and second mixer stages have for their sole objects to form said quadrature interference compensating signals. These interference compensating signals do then not only compensate for the oscillator interferences produced at the first and second mixer stages, but also the oscillator interference produced at the further mixer stage in the signal direction. This measure is, for example, advantageous for stereo decoders.

A further preferred embodiment of the last-mentioned mixer arrangement, is characterized by a frequency-dividing circuit arranged between the further mixer stage and the oscillator circuit.

The use of this measure prevents higher order interferences in the output signal of the further mixer stage which may be produced by a shift in the direct current setting (d.c. offset) and a higher harmonic in the (possibly discrete) mixing signal applied to the further mixer stage, cross-talk or leakage thereof or because of switching in-accuracies in the further mixing stage in case it is in the form of a time-discrete multiplier. The order of the interferences to be suppressed is adjustable by means of the frequency dividing factor of the frequency dividing circuit.

Another preferred embodiment of a mixer arrangement is characterized by a further mixer stage to which a mixing signal is applied from the oscillator circuit, an output of the third mixer

stage corresponding with an output of the mixer arrangement and an input being coupled to an input of the mixer arrangement via the superposition circuit.

When this measure is applied, the first and second mixer stages are again used only for forming said quadrature interference compensating signals and the further mixer stage only for signal processing, but in contrast with the last-mentioned preferred embodiments the total oscillator interference is suppressed in a direction opposite to the signal direction, as is, for example, desired in RF-input stages for the suppression of oscillator radiation.

The invention will now be described in greater detail, by way of example with reference to the Figures shown in the accompanying drawings, in which corresponding elements have been given the same references.

Therein:

Figure 1 shows a first embodiment of a mixer arrangement according to the invention for processing quadrature input signals in a receiver comprising a quadrature RF-tuning device preceding the mixer arrangement.

Figure 2 shows a second embodiment of a mixer arrangement which in a first mode of application is suitable for suppressing downstream oscillator interference and in a second mode of application for suppression of upstream oscillator interference.

Figure 3 shows a vector diagram associated with the mixer arrangement shown in Figure 1.

Figure 4 shows a vector diagram associated with the mixer arrangement shown in Figure 2.

Figure 1 shows a receiver having coupled to an aerial input A a quadrature RF-tuning device T having quadrature outputs, which are respectively connected to quadrature inputs I_1 and I_2 of a mixer arrangement M according to the invention, via low-pass filters LP and LP'. The quadrature RF-tuning device T comprises a pair of quadrature mixer stages M_{T0} and M_{T0}' , to which quadrature mixing signals are applied from a tuning oscillator TO and which converts a desired RF-receiving signal into a pair of low-frequency quadrature sub-signals.

These quadrature sub-signals are selected by means of said low-pass filters LP and LP' and in the mixer arrangement M applied to first and second mixer stages M_1 and M_2 via first and second subtracting circuits S_1 and S_2 still to be described. From an oscillator circuit FO quadrature mixing signals are applied to these mixer stages M_1 and M_2 , as a result of which the quadrature sub-signals are converted into in-phase and anti-phase signal components and are simultaneously subjected to a frequency translation. By adding these signal components together in a superposition circuit S_0 , the desired signal is obtained which, depending on the oscillation frequency of the oscillator circuits T_0 and F_0 may be located in the baseband or in an intermediate-frequency band. The desired signal thus obtained is applied via an output O, which is

common to the superposition circuit S_0 and the mixer arrangement M to a processing and reproducing arrangement P, in which in a manner known *per se* further processing and reproduction of the desired signal is effected.

The description of the signal processing given in the foregoing of the receiver shown is sufficient to understand the invention. For further details of this receiver, more specifically as regards the reception of single-sideband signals, reference is made to the above-mentioned article. Further details as regards the reception of TV and double-sideband AM signals are described in the Netherlands patent application NL-A-8 301 179 published 1/11/1984.

According to the invention, the mixer arrangement M also comprises first and second interference negative feedback paths (SD_1, LP_1, S_1) and (SD_2, LP_2, S_2), respectively which include first and second synchronous detectors SD_1 and SD_2 , respectively, signal inputs of which are coupled to the output O and carrier inputs to the oscillator circuit F_0 . Outputs of the synchronous detectors SD_1 and SD_2 are coupled to inverting inputs of the subtracting circuits S_1 and S_2 via first and second low-pass filters LP_1 and LP_2 , respectively. Non-inverting inputs of the subtracting circuits S_1 and S_2 are coupled to the low-pass filters LP and LP' , respectively and outputs thereof are coupled to inputs of the two mixer stages M_1 and M_2 , respectively.

Due to a shift in the direct current setting and/or oscillator cross-talk or leakage in or at the two mixer stages M_1 and M_2 so-called oscillator interferences occur in the signal at the outputs of these mixer stages M_1 and M_2 *in situ* of the oscillator frequency. Taking a quadrature relationship between the mixing signals of the two mixer stages M_1 and M_2 as a starting point, as shown by the system of co-ordinates in the vector diagram of Figure 3, these oscillator interferences in this vector diagram can be represented by interference factors $\bar{m}_1$ and $\bar{m}_2$, respectively. In the superposition circuit S_0 , which may optionally be formed by a junction point, a vectorial addition of these interference vectors $\bar{m}_1$ and $\bar{m}_2$ is effected, which results in a total or resultant interference sum vector $\bar{m}_1 + \bar{m}_2$.

In the embodiments shown, the quadrature carriers applied to the synchronous detectors SD_1 and SD_2 are in phase with the quadrature carriers applied to the mixer stages M_1 and M_2 and the first quadrature component $\bar{sd}_1$ of the total interference vector $\bar{m}_1 + \bar{m}_2$ is in phase with the mixing signal applied to the first mixer stage M_1 , and the second quadrature component $\bar{sd}_2$ is in phase with the mixing signal applied to the second mixer stage M_2 . These detected quadrature interference components $\bar{sd}_1$ and $\bar{sd}_2$ are subtracted in the subtracting circuits S_1 and S_2 from the quadrature input signals mentioned in the foregoing, after being selected in the first and second low-pass filters LP_1 and LP_2 . In this situation, the subtracting circuits S_1 and S_2 operate as inverter circuits for the respective quadrature interference

components $\bar{sd}_1$ and $\bar{sd}_2$, which are subjected therein to sign inversion. In the two mixer stages M_1 and M_2 the inverted quadrature interference components $-\bar{sd}_1$ and $-\bar{sd}_2$ are modulated on the oscillator frequency, and result in quadrature interference compensating signals which in the superposition circuit S_0 form an interference compensation sum vector $-(\bar{sd}_1 + \bar{sd}_2)$, which is equal to and of the opposite direction to the above-mentioned total interference vector $\bar{m}_1 + \bar{m}_2$. Depending on the open loop gain A in the interference negative feedback paths (SD_1, LP_1, S_1) and (SD_2, LP_2, S_2), respectively and the mixer stages M_1 and M_2 , respectively, the total interference vector $\bar{m}_1 + \bar{m}_2$ is suppressed by a vector of

$$\frac{1}{1+A}$$

It is obvious that an interference reduction already takes place at an open loop gain less than unity. However, for an effective interference suppression the said open loop gain A will in practice be chosen to be much higher than 1 and more specifically in such a way that an optimum ratio is reached between the loop band width and the stability.

To that end amplifier devices, not shown, can be included in an obvious manner in said two interference negative feedback paths (SD_1, LP_1, S_1) and (SD_2, LP_2, S_2).

It will further be clear that the subtracting circuits S_1 and S_2 can be replaced in a simple way by adder circuits or simple junction points, not shown, if inverter circuits, not shown, which are known *per se* are included in the signal paths before the subtractor circuits S_1 and S_2 , that is to say between the output O and the respective synchronous detectors SD_1 and SD_2 , it being possible to realize the inverter circuit by means of for example, delay circuits, or between the synchronous detectors SD_1, SD_2 and the subtracting circuits S_1, S_2 , respectively. Alternatively, a sign inversion can be obtained by means of an anti-phase relationship between the quadrature carrier applied to the synchronous detectors SD_1 and/or SD_2 on the one hand and the mixing signal applied to the mixer stages M_1 and/or M_2 , respectively. Starting from reference quadrature phases 0° and 90° for the two quadrature mixing signals, the phases of the two carriers can then, for example, be 180° and 270° . As a result thereof the above-mentioned inverted quadrature noise components $-\bar{sd}_1$ and $-\bar{sd}_2$ are then directly obtained at the outputs of the synchronous detectors SD_1 and SD_2 . Such an implementation, not shown, is possible if, for example, the oscillator circuit F_0 is of a push-pull construction, quadrature oscillator signals being available in pairs and in anti-phase.

Figure 2 shows a second embodiment of a mixer arrangement M according to the invention having first and second terminals I/O and O/I, respectively and a further mixer stage M_0 con-

nected therebetween. A mixing signal input of this mixer stage M_0 is coupled to an output of the oscillator circuit F_0 via a frequency dividing circuit D, still further to be described, and, depending on the frequency dividing factor N of the frequency dividing circuit D, its frequency may be equal to once or a factor of $1/N$ times the oscillator frequency, where $N=2, 3, 4 \dots$. Similar to the output O of the embodiment shown in Figure 1, the second terminal O/I is coupled to an output of the superposition circuit S_0 , which is in the form of a junction point, while for a sign inversion of the quadrature noise components $\overline{sd}_1'$ and $\overline{sd}_2'$, still further to be described, inverter circuits S_1' and S_2' , which are known *per se* are used instead of the said subtracting circuits S_1 and S_2 .

For an interference suppression in the signal direction, that is to say a downstream suppression of interferences in the output signal of the further mixer stage M_0 , the first terminal I/O functions as the input and the second terminal O/I as the output of both the mixer arrangement M and the further mixer stage M_0 . If a suppression of interferences in the output signal of the mixer arrangement M at the frequency of the mixing signal applied to the further mixer stage M_0 is desired, which is, for example, the case in stereo decoders, then the frequency dividing factor is 1. In that case the frequency dividing circuit D has no function and may be omitted or optionally be short-circuited.

The oscillator interference in the output signal of the further mixer stage M_0 is shown in the vector diagram of Figure 4 by way of example with the aid of an interference vector $\overline{m}_3$. In the junction point S_0 , which functions as a superposition circuit this interference vector $\overline{m}_3$ is added to the interference sum vector $\overline{m}_1 + \overline{m}_2$, already described in the foregoing, of the oscillator interferences in the output signals of the first and second mixer stages M_1 and M_2 . This addition results in a new total interference sum vector $\overline{m}_1 + \overline{m}_2 + \overline{m}_3$ whose quadrature interference components $\overline{sd}_1'$ and $\overline{sd}_2'$ in the respective phase directions of the quadrature mixing signals applied to the first and second mixer stages M_1 and M_2 are detected in the two synchronous detectors SD_1 and SD_2 , respectively. In correspondence with what has already been described in the foregoing for the quadrature interference components $\overline{sd}_1$ and $\overline{sd}_2$, quadrature interference compensating signals are formed by inversion and modulation, whose vectorial sum $-(\overline{sd}_1' + \overline{sd}_2')$ in the junction point S_0 is equal to and oppositely directed to the total interference sum vector $\overline{m}_1 + \overline{m}_2 + \overline{m}_3$ and suppresses it in dependence on the negative feedback gain, at least to a significant extent.

If a suppression of higher order interferences in the output signal of the mixer arrangement M is desired, for example interferences *in situ* of the n^{th} harmonic of the mixing signal of the further mixer stage M_0 such as may occur, for example, more specifically in time-discrete mixing processes in the further mixer stage M_0 when formed

as a discrete multiplier circuit, then the oscillator frequency must amount to n times the frequency of the said mixing signal and the frequency dividing circuit D must be adjusted to a frequency-dividing factor n . A negative feedback and suppression of the last-mentioned n^{th} order interferences is effected via the interference negative feedback paths (SD_1, LP_1, S_1') and (SD_2, LP_2, S_2') and the two mixer stages M_1 and M_2 .

It will be obvious that combinations of higher order interferences can be suppressed by means of combinations of pairs of interference negative feedback paths and mixer stages. Thus, it is very well possible to suppress both the 1st and the 3rd-order interferences in the output signal of the further mixer stage M_0 . To that end the oscillator frequency must correspond to the highest of the noise frequencies to be suppressed, that is to say three times the frequency of the mixing signal of the further mixing stage M_0 , and the frequency dividing factor of the frequency dividing circuit D must be 3. The frequency dividing circuit D must then be capable of producing in a manner known *per se*, in addition to an output signal to be applied as a mixing signal to the further mixer stage M_0 a signal which with respect thereto is a quadrature output signal. These two quadrature output signals must be applied as quadrature mixing signals to third and fourth mixer stages, not shown, and as quadrature carriers to third and fourth synchronous detectors, also not shown, of third and fourth interference negative feedback paths, to suppress the 1st order interferences in the output signal of the further mixer stage M_0 . These third and fourth mixer stages and interference negative feedback paths must then be connected with respect to each other in the same way as the mixer stages M_1 and M_2 and the interference negative feedback parts (SD_1, LP_1, S_1') and (SD_2, LP_2, S_2') , which is not shown. Their junction point, which functions as a superposition circuit, must then be coupled to the junction point S_0 .

For suppressing an upstream interference, that is an interference in a direction which is opposite to the signal direction, e.g. in the input signal of the mixer arrangement M shown in Figure 2, for example for reducing oscillator radiation, the first terminal I/O functions as an (IF-) output and the second terminal O/I as an (aerial) input of the mixer arrangement M and the further mixer stage M_0 . The frequency dividing circuit D then has the same function as in the application described in the foregoing, which may be omitted or optionally short-circuited if only the suppression of oscillator radiation is desired. The suppression of oscillator radiation proceeds in all respect in correspondence with the above-described suppression of the noise vector $\overline{m}_3$.

It should be noted that the invention is not limited to the shown and described embodiments. It is, for example, highly possible, while applying the inventive idea, to substitute a subtracting circuit in combination with a suitably chosen signal sign inversion in one or both

interference negative feedback paths as a superposition circuit S_0 for an adder circuit or junction point.

It is alternatively possible to use in the embodiment shown in Figure 2 a frequency multiplier circuit instead of the frequency dividing circuit D for suppressing an n^{th} order interference. The oscillator frequency must then correspond to the mixing frequency in the further mixer stage M_0 and must be applied in a phase-quadrature relationship to the two first and second synchronous detectors and to the two first and second mixer stages after the frequency has been multiplied by a factor of n in the said frequency multiplying circuit.

Claims

1. A mixer arrangement comprising first and second mixer stages, to which quadrature mixing signals are applied from an oscillator circuit, these two mixer stages being coupled to a superposition circuit, characterized by first and second quadrature interference negative feedback paths for a negative feedback of oscillator frequency-coupled interferences from an output of the superposition circuit to inputs of the two mixer stages, comprising first and second synchronous detectors, respectively coupled to the output of the superposition circuit and also via first and second low-pass filters to inputs of the first and second mixer stages, quadrature carriers which are in an in-phase or an anti-phase relationship with the quadrature mixing signals being applied to these synchronous detectors from the oscillator circuit, whereas for the case in which there is an in-phase relationship between at least one of the said carriers and one of the said mixing signals the interference negative feedback path in which the synchronous detector which is fed by the last-mentioned carrier is included also comprises an inverter circuit for inverting the sign of the signal.

2. A mixer arrangement as claimed in Claim 1, characterized by an in-phase relationship between the two carriers and the two mixing signals, by first and second subtracting circuits whose inverting inputs are coupled to the first and second low-pass filters, respectively, whose non-inverting inputs are coupled to first and second quadrature inputs of the mixer arrangement, respectively and whose outputs are coupled to the inputs of the first and the second mixer stages, respectively and in that the output of the superposition circuit is connected to an output of the mixer arrangement.

3. A mixer arrangement as claimed in Claim 1, characterized by a further mixer stage to which a further mixing signal is applied from the oscillator circuit, an input of the mixer arrangement being coupled to an input of the third mixer stage and an output of the third mixer stage being connected to an input of the superposition circuit.

4. A mixer arrangement as claimed in Claim 3, characterized by a frequency-dividing circuit

arranged between the further mixer stage and the oscillator circuit.

5. A mixer arrangement as claimed in Claim 1, characterized by a further mixer stage to which a mixing signal is applied from the oscillator circuit, an output of the third mixer stage being coupled to an output of the mixer arrangement and an input being coupled to an input of the mixer arrangement via the superposition circuit.

Patentansprüche

1. Mischeranordnung mit ersten und zweiten Mischstufen, denen aus einer Oszillatorschaltung Quadraturmischsignale zugeführt werden, wobei diese beiden Mischstufen an eine Überlagerungsschaltung angeschlossen sind, gekennzeichnet durch erste und zweite Quadraturstörgegenkoppelwege für eine Gegenkopplung mit der Oszillatorfrequenz gekoppelter Störungen von einem Ausgang einer Überlagerungsschaltung auf Eingänge der beiden Mischstufen, mit ersten bzw. zweiten Synchrondetektoren, die einerseits an den Ausgang der Überlagerungsschaltung und andererseits über erste und zweite Tiefpassfilter an Eingänge der ersten und zweiten Mischstufen angeschlossen sind, wobei diesen Synchronisationsdetektoren von der Oszillatorschaltung zu den Quadraturmischsignalen gleichphasige oder gegenphasige zugeführten Quadraturträgern werden, wobei bei Phasengleichheit zwischen wenigstens einem der genannten Träger und einem der genannten Mischsignale der Störgegenkoppelweg, in den der vom letztgenannten Träger gespeiste Synchronisationsdetektor aufgenommen ist, ebenfalls eine Umkehrschaltung für eine Vorzeichenumkehr des Signals enthält.

2. Mischeranordnung nach Anspruch 1, dadurch gekennzeichnet dass die beiden Träger und die beiden Mischsignale phasengleich sind, dass erste und zweite Subtraktionsschaltungen mit ihren invertierenden Eingängen an die ersten bzw. zweiten Tiefpassfilter, mit ihren nicht invertierenden Eingängen an erste bzw. zweite Quadratureingänge der Mischeranordnung und mit ihren Ausgängen an die Eingänge der ersten bzw. der zweiten Mischstufe angeschlossen sind, und dass der Ausgang der Überlagerungsschaltung mit einem Ausgang der Mischeranordnung verbunden ist.

3. Mischeranordnung nach Anspruch 1, gekennzeichnet durch eine weitere Mischstufe, der aus der Oszillatorschaltung ein weiteres Mischsignal zugeführt wird, wobei ein Eingang der Mischeranordnung an einen Eingang der dritten Mischstufe angeschlossen und ein Ausgang der dritten Mischstufe mit einem Eingang der Überlagerungsschaltung verbunden ist.

4. Mischeranordnung nach Anspruch 3, gekennzeichnet durch eine zwischen der weiteren Mischstufe und der Oszillatorschaltung angeordnete Frequenzteilerschaltung.

5. Mischeranordnung nach Anspruch 1, gekennzeichnet durch eine weitere Mischstufe,

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interference negative feedback paths as a superposition circuit S_0 for an adder circuit or junction point.

It is alternatively possible to use in the embodiment shown in Figure 2 a frequency multiplier circuit instead of the frequency dividing circuit D for suppressing an n^{th} order interference. The oscillator frequency must then correspond to the mixing frequency in the further mixer stage M_0 and must be applied in a phase-quadrature relationship to the two first and second synchronous detectors and to the two first and second mixer stages after the frequency has been multiplied by a factor of n in the said frequency multiplying circuit.

Claims

1. A mixer arrangement comprising first and second mixer stages, to which quadrature mixing signals are applied from an oscillator circuit, these two mixer stages being coupled to a superposition circuit, characterized by first and second quadrature interference negative feedback paths for a negative feedback of oscillator frequency-coupled interferences from an output of the superposition circuit to inputs of the two mixer stages, comprising first and second synchronous detectors, respectively coupled to the output of the superposition circuit and also via first and second low-pass filters to inputs of the first and second mixer stages, quadrature carriers which are in an in-phase or an anti-phase relationship with the quadrature mixing signals being applied to these synchronous detectors from the oscillator circuit, whereas for the case in which there is an in-phase relationship between at least one of the said carriers and one of the said mixing signals the interference negative feedback path in which the synchronous detector which is fed by the last-mentioned carrier is included also comprises an inverter circuit for inverting the sign of the signal.

2. A mixer arrangement as claimed in Claim 1, characterized by an in-phase relationship between the two carriers and the two mixing signals, by first and second subtracting circuits whose inverting inputs are coupled to the first and second low-pass filters, respectively, whose non-inverting inputs are coupled to first and second quadrature inputs of the mixer arrangement, respectively and whose outputs are coupled to the inputs of the first and the second mixer stages, respectively and in that the output of the superposition circuit is connected to an output of the mixer arrangement.

3. A mixer arrangement as claimed in Claim 1, characterized by a further mixer stage to which a further mixing signal is applied from the oscillator circuit, an input of the mixer arrangement being coupled to an input of the third mixer stage and an output of the third mixer stage being connected to an input of the superposition circuit.

4. A mixer arrangement as claimed in Claim 3, characterized by a frequency-dividing circuit

arranged between the further mixer stage and the oscillator circuit.

5. A mixer arrangement as claimed in Claim 1, characterized by a further mixer stage to which a mixing signal is applied from the oscillator circuit, an output of the third mixer stage being coupled to an output of the mixer arrangement and an input being coupled to an input of the mixer arrangement via the superposition circuit.

Patentansprüche

1. Mischeranordnung mit ersten und zweiten Mischstufen, denen aus einer Oszillatorschaltung Quadraturmischsignale zugeführt werden, wobei diese beiden Mischstufen an eine Überlagerungsschaltung angeschlossen sind, gekennzeichnet durch erste und zweite Quadraturstörgegenkoppelwege für eine Gegenkopplung mit der Oszillatorfrequenz gekoppelter Störungen von einem Ausgang einer Überlagerungsschaltung auf Eingänge der beiden Mischstufen, mit ersten bzw. zweiten Synchrondetektoren, die einerseits an den Ausgang der Überlagerungsschaltung und andererseits über erste und zweite Tiefpassfilter an Eingänge der ersten und zweiten Mischstufen angeschlossen sind, wobei diesen Synchronisationsdetektoren von der Oszillatorschaltung zu den Quadraturmischsignalen gleichphasige oder gegenphasige zugeführten Quadraturträgern werden, wobei bei Phasengleichheit zwischen wenigstens einem der genannten Träger und einem der genannten Mischsignale der Störgegenkoppelweg, in den der vom letztgenannten Träger gespeiste Synchronisationsdetektor aufgenommen ist, ebenfalls eine Umkehrschaltung für eine Vorzeichenumkehr des Signals enthält.

2. Mischeranordnung nach Anspruch 1, dadurch gekennzeichnet dass die beiden Träger und die beiden Mischsignale phasengleich sind, dass erste und zweite Subtraktionsschaltungen mit ihren invertierenden Eingängen an die ersten bzw. zweiten Tiefpassfilter, mit ihren nicht invertierenden Eingängen an erste bzw. zweite Quadratureingänge der Mischeranordnung und mit ihren Ausgängen an die Eingänge der ersten bzw. der zweiten Mischstufe angeschlossen sind, und dass der Ausgang der Überlagerungsschaltung mit einem Ausgang der Mischeranordnung verbunden ist.

3. Mischeranordnung nach Anspruch 1, gekennzeichnet durch eine weitere Mischstufe, der aus der Oszillatorschaltung ein weiteres Mischsignal zugeführt wird, wobei ein Eingang der Mischeranordnung an einen Eingang der dritten Mischstufe angeschlossen und ein Ausgang der dritten Mischstufe mit einem Eingang der Überlagerungsschaltung verbunden ist.

4. Mischeranordnung nach Anspruch 3, gekennzeichnet durch eine zwischen der weiteren Mischstufe und der Oszillatorschaltung angeordnete Frequenzteilerschaltung.

5. Mischeranordnung nach Anspruch 1, gekennzeichnet durch eine weitere Mischstufe,



der aus der Oszillatorschaltung ein Mischsignal zugeführt wird, wobei ein Ausgang der dritten Mischstufe an einen Ausgang der Mischeranordnung und ein Eingang über die Überlagerungsschaltung an einen Eingang der Mischeranordnung angeschlossen sind.

Revendications

1. Dispositif mélangeur comprenant un premier et un second étage mélangeur, auxquels des signaux de mélange en quadrature sont appliqués à partir d'un circuit oscillateur, ces deux étages mélangeurs étant couplés à un circuit de superposition, caractérisé par un premier et un second trajet de contre-réaction d'interférence en quadrature pour une contre-réaction d'interférence couplée en fréquence d'oscillateur à partir d'une sortie du circuit de superposition vers des entrées de deux étages mélangeurs, comprenant un premier et un second détecteur synchrone couplés respectivement à la sortie du circuit de superposition et, par l'intermédiaire d'un premier et d'un second filtre passe-bas, aux entrées du premier et du second étage mélangeur, des porteuses en quadrature qui sont en phase ou en opposition de phase avec les signaux de mélange en quadrature étant appliqués à ces détecteurs synchrones à partir du circuit d'oscillateur, tandis que pour le cas dans lequel où il existe une relation en phase entre au moins une des porteuses et un des signaux de mélange, le trajet de réaction négative d'interférence dans lequel le détecteur synchrone alimenté par la porteuse mentionnée en dernier lieu est incorporé, com-

prend également un circuit inverseur pour inverser le signe du signal.

2. Dispositif mélangeur suivant la revendication 1, caractérisé par une relation en phase entre les deux porteuses et les deux signaux de mélange, par un premier et un second circuit soustracteur dont les entrées inverseuses sont couplées au premier et au second filtre passe-bas respectivement, dont les entrées non inverseuses sont couplées à une première et une seconde entrée en quadrature du dispositif mélangeur respectivement et dont les sorties sont couplées aux entrées du premier et du second étage mélangeur respectivement et en ce que la sortie du circuit de superposition est connectée à une sortie du dispositif mélangeur.

3. Dispositif mélangeur suivant la revendication 1, caractérisé par un autre étage mélangeur auquel un autre signal de mélange est appliqué depuis le circuit oscillateur, une entrée du dispositif mélangeur étant couplée à une entrée du troisième étage mélangeur et une sortie du troisième étage mélangeur étant connectée à une entrée du circuit de superposition.

4. Dispositif mélangeur suivant la revendication 3, caractérisé par un circuit diviseur de fréquence disposé entre l'autre étage mélangeur et le circuit oscillateur.

5. Dispositif mélangeur suivant la revendication 1, caractérisé par un autre étage mélangeur auquel un signal de mélange est appliqué à partir du circuit oscillateur, une sortie du troisième étage mélangeur étant connectée à une sortie du dispositif mélangeur et une entrée étant connectée à une entrée du dispositif mélangeur par l'intermédiaire du circuit de superposition.

