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STABILISED POWER SUPPLY FOR SUPPLYING ALTERNATING
CURRENT POWER TO A CRITICAL LOAD

5 There are many applications in which it is
becoming increasingly important to assure that
equipment will be supplied with an uninterrupted
AC supply voltage, and that this voltage will be
a substantially pure and substantially noise-free
sinewave of predetermined fixed frequency. The
usual utility power lines are intended to provide
10 such a supply voltage, but are subject to complete
power outages, to reduction in voltage level, to
surges which cause the voltage to raise above the
normal level and to various types of interfering
noise picked up by the power lines.

15 For many purposes such inadequacies of the
power lines are relatively harmless, or at most
inconvenient. However, with other more critical
loads, for example computer apparatus, any of the
foregoing departures of the power line from a
20 constant, fixed-frequency, substantially noise-free
sinewave both "normal" and "common" mode can cause
loss of stored information and/or improper handling
of information by the load apparatus, either of
which can have very serious deleterious results.

25 Various types of power supply systems have been
proposed in the prior art which will operate, in one
degree or another, to mitigate one or more of the

foregoing defects in the line voltage supply. One of these is the so-called uninterruptible power supply (UPS) equipment and employs a battery charger, a battery and an inverter connected in tandem with each other, the charger being supplied from the AC power line and the inverter supplying AC to the computer or other critical load. The power line keeps the battery adequately charged despite small over-voltages, under-voltages or interfering noise of the utility line, and the inverter utilizes the stored energy of the battery to produce substantially pure single-frequency sinewaves of constant amplitude for supply to the critical load. In the event of long term power line failure, the battery and inverter will maintain the desired AC current and voltage at the load for a substantial period of time, after which discharge of the battery can be detected and the equipment appropriately shut down, its use discontinued, or other protective measure taken, such as shifting to other standby power.

While quite effective for its purpose, there are times when unusual load demands are placed on the inverter portion of the UPS. Since the inverter has a finite impedance, the output voltage will sag when heavy loads such as motor starting or load short that may happen from time to time. During these heavy load demands the output voltage will drop to unacceptable levels. To solve this problem UPS equipment will bypass the load, i.e., disconnect the load from the UPS inverter output and connect it to an alternate source (bypass source) that has

several orders of magnitude lower source impedance to supply the heavy load demands required without sagging the output voltage. The problem with bypass is that the load is now operating from the very source that prompted the use of the UPS in the first place. Experience has shown that modern computers and other sensitive equipment are more susceptible to the common mode noise than to the normal mode noise from the fluxuating utility.

Accordingly, a primary object of the present invention is to provide an improved stabilised power supply system.

Another object of the present invention is to provide an efficient power supply and line conditioner which provides the desired alternating-current voltage for the critical load, yet does not require a separate charger and inverter and therefore is more efficient and less expensive than those systems which require such apparatus.

The present invention is a stabilized power supply for supplying alternating current power to a critical load, such as a computer, comprising transformer means including an output winding connected with the load, and first, second and third input windings, first supply means including a battery and an inverter for supplying alternating-current power, second supply means for supplying alternating-current power, transfer switch means having first and second conditions for alternately connecting and disconnecting said first supply means and said first input winding for the supply of power to the load and for disconnecting and connecting said second supply means and said second input winding for the supply of power to the load, respectively, means connecting said third input winding with a third power supply means, and means affecting the vector relationship between the voltages of said third and first supply means to cause the real component of the inverter current at the break-even condition to be a minimum.

Uninterruptible power supply and line conditioner systems have been developed recently in which the utility line is coupled to the load and to the inverter output by way of series inductance, and in which the inverter comprises a bidirectional pulse-width modulation (PWM) sinewave inverter connected between the battery and the load. In such systems the phase of the sinewave generated can be varied as desired with respect to the phase of the utility line voltage, thereby varying the magnitude and phase of the contribution of the inverter current to the load current. In a typical operation, this phase angle may be set, and preferably automatically maintained, at a value sufficient to supply the power demanded by the load, plus any losses in the system, plus any amount of power which it is desired to supply to the battery to maintain it charged or to recharge it.

Typically, the magnitude of the alternating-current voltage supplied to the load from the utility line, and hence also supplied to the output terminals of the inverter, is substantially equal to the utility line voltage itself. Thus where the coupling between the inverter output, the load terminals and the utility line terminals is by way of three corresponding windings of a transformer, the ratio of the turns of the winding connected to

the utility line is equal to the number of turns coupled to the load terminals; that is, the ratio of the turns is 1:1 based on the concept that the load equipment is to be supplied with the same alternating voltage as is present on the power lines. While this arrangement will operate, it has been found that, for reasons set forth hereinafter, such a system, during normal "break even" operation, has its minimum inverter current under zero load conditions, and with a load present has a substantially greater-than-minimum inverter current; with a lagging load power factor, the required inverter current (and consequent inverter size) can become very great, and the system is therefore unduly expensive. Furthermore, its through-put efficiency is, in general, not the maximum obtainable.

Embodiments of the present invention will now be described, by way of example, with reference to the accompanying drawings, in which:-

Fig. 1 is a block diagram of a power supply system of the prior art including an inverter for supplying a stabilized alternating-current voltage to a critical load;

Fig. 2 is a block diagram of a basic power supply system including transformer means having an isolated bypass winding for coupling the power sources with the load;

Fig. 3 is a block diagram of a modification of the power supply system of Fig. 2, including inductance means connected in series in the utility line for power factor control;

Fig. 4 is an equivalent electrical circuit diagram of the system of Fig. 3;

Figs. 5 and 6 are vector diagrams illustrating the operation of the apparatus of Figs. 3 and 4;

Fig. 7 is a graph illustrating inverter current plotted against utility supply voltage;

Fig. 8 is an electrical equivalent circuit illustrating the voltage step-up provided by the transformer coupling means;

Fig. 9 is a graph illustrating through-put efficiency plotted against utility supply voltage;

Figs. 10A and 10B are electrical circuit diagrams of power supply systems according to the present invention illustrating power factor control by the use of separate inductance means and transformer shunt means, respectively;

Fig. 11 is a schematic electrical diagram of the preferred embodiment of the invention;

Fig. 12 is a diagrammatic illustration of the coupling of the transformer windings of the apparatus of Fig. 11;

Figs. 13A and 13B are vector diagrams further illustrating the operation of the invention of Fig. 11;

Fig. 14 is a block diagram of a system incorporating the power supply of the present invention; and

Figs. 15A and 15B are waveform diagrams illustrating the bidirectional line conditioning obtained by the system of the present invention.

Referring first to the system of the prior art illustrated diagrammatically in Fig. 1, the alternating-current utility or supply voltage source 10 is connected with a rectifier/charger 12 which converts the alternating-current voltage to a direct-current voltage so as to charge a battery 16. The voltage across the latter battery is then utilized to operate an inverter 18, which converts the DC voltage of the battery to an alternating-current voltage and supplies it via transfer switch 19 and output line 22 to the critical AC load 23. With this system, the utility line can be disconnected for substantial periods while the inverter continues to supply the desired alternating voltage, while at the same time substantial protection is provided against interfering noise, current surges, momentary voltage drops and irregularities in the waveform of the utility line voltage. In the event a heavy load occurs when the bypass source 14 is available, the unit will transfer load to bypass 14 via transfer switch 19.

Fig. 2 is similar to Fig. 1, but a transformer 20 provides means for alternately coupling the inverter or bypass sources with the critical load, respectively. The transformer 20 serves to provide different bypass and utility voltages as well as providing a different critical load voltage. The transfer switch 19 defines the means for rapidly changing the source of power.

Fig. 3 is a diagram illustrating a modification of Fig. 2. In this case the utility line 24 supplies alternating-current voltage to the four-quadrant pulse width modulated sinewave inverter 26 via a series inductor 27, and the output of the inverter is connected via the transformer coupling means 28 to the critical load 23. The battery 30 is connected to the inverter, and the inverter determines how much of the critical load current is supplied from the utility line and how much from the battery, and how much of the inverter current is supplied to charge the battery.

This figure is shown in normal operation; when operating in the bypass mode the transfer switch 19 is closed to connect bypass source 14 with the transformer coupling means 28, and to simultaneously disconnect the utility source 24.

Fig. 3 represents an improvement in the general type of system illustrated in Fig. 2.

The construction and operation of a system in accordance with Fig. 3 will now be explained and described, after which the improvement thereon according to the present invention will be set forth in greater detail.

Fig. 4 is a simplified equivalent circuit for the general arrangement of Fig. 3, depicting the utility line voltage E_U , the series inductance L_S

through which the current I_i flows, and the critical load Z_o to which the load current I_o is supplied. The inverter and critical load are effectively in parallel with each other, and supplied with voltage from the utility line 24 by way of series inductor L_s .

The generalized phase diagram for such a circuit is shown in Fig. 5 for the case in which the angle between the utility line voltage E_u and the inverter output voltage E_i is β , with the inverter voltage lagging. The voltage E_L across the inductance is the vector difference between the vectors E_u and E_i , and hence is a vector joining the heads of the vectors of the latter two quantities, as shown. The inductance current I_L , for a substantially lossless inductance, is at right angles to E_L and the load current I_o is assumed to lag the inverter voltage by a load power factor angle θ . The inverter current I_i is equal to the vector difference between the load current I_o and the inductance current I_L , as shown in the drawing. Also shown is the angle α by which I_L lags E_u .

Fig. 6 illustrates the effects produced by changing the angle β between the utility line voltage E_u and the inverter output voltage E_i ; the magnitudes of E_u and E_i are equal, and for simplicity the case is shown wherein the load power factor is unity.

As shown, when β is small (e.g. $\beta = \beta_1$), the input or inductor current I_{L1} is also small; the inverter current I_{i1} is nearly in phase with the

inverter voltage E_i and therefore the inverter is delivering real power to meet the power requirements of the load not supplied by the utility line; thus, in this case the inverter battery is discharging.

5 When β is somewhat larger ($\beta = \beta_2$), I_{L2} is considerably larger and, in fact, its real part (i.e. its projection along the horizontal axis) is equal to I_0 , and the utility supplies all of the load power. Since I_{i2} is at 90° to the inverter
10 voltage E_i , no real power flows into or out of the inverter and therefore the battery current is zero (ignoring losses). However, there is a substantial reactive current in the inverter, as depicted by the vector I_{i2} . This condition in which substantially
15 no real power flows in or out of the inverter we designate as the "break even" case.

For a still larger input voltage displacement angle ($\beta = \beta_3$), I_{L3} is substantially larger, as is the inverter current I_{i3} ; however, the direction of
20 the vector I_{i3} indicates that real power is flowing into the inverter, while the inverter battery is being charged during such operation at the angle β_3 .

As is seen from Fig. 6, varying the input displacement angle β significantly changes the magnitude of the inverter current I_i . Table 1 hereof
25 summarizes the variation of β and I_i for different full load power factors and values of input inductance (L_S). This table was computed assuming an 83% efficient inverter for both the "break even" (bat-
30 tery charging current and real inverter power = 0)

and "battery charging" (charge current or real inverter power = 0.2 P.U.) cases, wherein P.U. indicates per unit, i.e. all parameters including inductance have been normalized to the load voltage and current.

The input voltage displacement angle β for any given load, input voltage, and charge current condition increases with increasing value of the inductance L_S . However, at -15% utility voltage ($E_U = 0.85$), inverter current is minimal when L_S equals 0.4 P.U. At this optimal inductance value, the inverter still must be sized to handle 130% full load current (at "break even") when the load power factor is 0.8 lagging. Moreover, to charge the battery under these conditions requires an inverter rated at 150%.

Fig. 7 illustrates the variation of inverter current as a function of input voltage (normalized), at the break-even operation condition. It is noted that for unity power factor, inverter current is minimum when the input or utility voltage E_U is equal to 1.1 P.U.

Fig. 8 shows a system in equivalent current form, with a step-up of 1 to 1.1 in voltage between the line voltage terminals and the input to the inductance L_S , (in

this equivalent circuit, shown as if it were provided by an auto transformer connection). At this ratio of 1.1, inverter current at no load is actually higher than a full load, as indicated by the arrow a in Fig. 7.

Table 2 shows the reduction in the required inverter current when the input voltage has been transformed by the 1.1 ratio. Included in this Table is the input power factor angle α between E_U and I_L . As indicated, the input power factor actually improves at -15% line voltage, viz, when $E_U = 0.935 (1.1 \times 0.85)$.

The effect of transforming the input voltage in this manner is further illustrated in Fig. 9, wherein the through-put efficiency is plotted as ordinate and the normalized utility voltage E_U is plotted as abscissa, for an 83% efficient inverter. Throughput efficiency is maximum approximately when the inverter current is minimum, at a transformed input voltage of about 1.1. The values indicated were calculated for a 120-volt, 3 kilovolt-ampere system. From this it will be seen that, for a unity power-factor load, the 1.1 ratio gives substantially maximum through-put efficiency, and gives reasonable efficiencies for both 0.8 lag power factor and 0.9 lead power factor. For other loads having different power factors, maximum through-put and minimum "break-even" inverter current may be obtained by using other suitable ratio values.

Fig 10A is a diagram similar to Fig. 3 but illustrating a first embodiment of the present invention. In this case the utility line 24 supplies alternating voltage to the four-quadrant PWM sinewave inverter 26 via a series inductance 25, and the output of the inverter is connected through the transformer coupling means 28 to the critical load 22. The battery 30 is connected with the inverter 26, and the inverter determines how much of the critical load current is supplied from the utility line and how much from the battery, and how much of the inverter current is supplied to charge the battery.

The system of this figure is shown in its normal operating condition. When operating in the bypass mode, the transfer switch 19 is operated, whereby bypass source 14 is connected with the transformer coupling means 28, utility source 24 is disconnected from winding 76 and the inverter is connected to the coupling means through $N_T L_S$ inductor 27 that is sized to reflect the turns ratio of the coupling means so as to appear to the inverter exactly as before when operating from the utility 24 with inductor 25. This enables the inverter to recharge and maintain the battery at the desired level even when the load is connected with the bypass source.

In the modification of Fig. 10B, instead of providing an inductor L_S , magnetic shunts M having the same effective inductance are inserted in the



transformer coupling 28. The critical load winding 80, inverter winding 78 and bypass winding 112 are tightly coupled together, the utility source winding 76 being loosely coupled to the other windings. The degree of coupling is selected to be equivalent to the discrete inductor L_S of Fig. 10A.

The system has been discussed above predominately with equal voltages in and out. The transformer enables one to convert one AC voltage to another, as is well known in the art. However, when the voltage ratio is changed for the input winding of the machine, the value of L_S is automatically scaled to the correct value required by the input voltage. It is equally possible to alter any one of the windings of the transformer to produce any desired critical load voltage from any input voltage and in event of a heavy load demand bypass to an alternate source of a third voltage, if desired.

Turning now to Fig. 11, there is shown a preferred embodiment of the invention for the typical case of utility voltage of 120 volts AC, a load voltage of 120 volts AC, a load power requirement of three KVA at 60 hz, and a load power factor of unity. A battery 40, in this example providing 120 volts DC, is connected via an appropriate fuse 42 to a shunt capacitor 44, typically having a value of about 15,000 microfarad. Also connected across the battery is the four-quadrant PWM sinewave inverter 46 made up of the PWM filter 48 and the four transistor-diode sections A, B, C and D arranged in a

bridge configuration, where the battery is connected between the top and bottom junctions 50, 52 of the bridge and the opposed side junctions 54 and 56 of the bridge are connected with the respective input lines 58 and 60 of the PWM filter. Each of the bridge sections A, B, C and D is made up of a high current NPN switching transistor having a high-current semiconductor diode in parallel therewith.

In each of the upper sections A and C of the bridge, the collectors of the two transistors are connected with the positive side of the battery, and the emitters are connected with bridge output lines 58 and 60, respectively. The two diodes in the upper sections A and C are poled so that their cathodes are connected with the positive end of the battery, and the transistors and diodes in the lower bridge sections B and D are poled oppositely from those in sections A and C. Such circuits and their operation are well known in the art for use as PWM inverters. In such operation, the bases of the four switching transistors are turned ON and OFF in pairs in a predetermined sequence at predetermined times and for predetermined intervals (in this example, 26 times per sinewave cycle), so that the output leads 58 and 60 of the bridge circuit are provided with pulse-width modulated pulse signal having energies representing a sinewave, which signal after passage through the low-pass PWM filter 48 therefore produces a sinewave in response to energy from the battery. In a typical case, each of the capacitors

C_T and C_F of the filter may have a value of about 200 microfarad, the inductance of each of the two coils L_F may be about 400 microhenries and the inductance of the coil L_T may be about 13 microhenries, producing a low-pass filter having an upper band limit at about 3 KHz and a rejection trap at the carrier frequency of the PWM pulses. The output terminals 70, 72 of the inverter are connected across the inverter winding 78 of a transformer 84 via transfer switch 19. In a typical case, the transformer winding 78 may have a number of turns equal to about $1/2$ of the number of turns of the load winding 80 which supplies power to the load (that is, if the number of turns of winding 80 is N_2 then the number of turns of inverter output winding 78 equals $1/2 N_2$). During bypass operation, the utility line is connected to winding 112 through a static switch means 120. In the typical case transformer winding 112 has the same number of turns as winding 80. Also in the bypass mode, the inverter is connected with transformer winding terminals 71 and 72 through AC switch means 60 and inductor 61, permitting the inverter to operate from winding 78 of transformer 84 as if it were the utility line.

Transformer windings 112, 78 and 80 are tightly coupled to each other, e.g., may be wound one on top of the other on a common iron core 84 so that the inverter output voltage is the load voltage. Transformer winding 80 is connected directly to the load input terminals 88 and 90. All static switches 120,

60 and 122 are used to permit more rapid switching from the UPS unit to the alternate sources. They are made up of a pair of parallel, oppositely-poled silicon-controlled-rectifiers each of which can be triggered on by signals applied to its gate electrode, the pair thus serving as a bidirectional electronic switch, operable in response to electrical signals indicative of any selected malfunction, such as a large change in load voltage due to load voltage due to a load disturbance.

The portion of Fig. 11 thus far described in detail represents, in its general form, a known type of inverter system for operating a critical AC load from a battery and for charging the battery from an AC source, and hence need not be described in even further detail.

The AC utility line, made up of the high line 96 and the neutral line 98 is connected, via utility line input terminals 108 and 110, to transformer winding 76, which is located on the same core as the windings 112, 80 and 78 but is loosely coupled thereto by virtue of the intervening magnetic shunts 114 and 116, which typically comprise bodies of ferro-magnetic material positioned to shunt or bypass a portion of the magnetic flux which otherwise would extend between coil 76 and the coils 112, 80 and 78; each magnetic shunt is designed to provide at least a small air gap on each side of the shunt so that complete shunting does not occur. Such constructions and procedures are well known in

the art and need not be described herein in detail, and a physical arrangement of such a transformer is illustrated schematically in Fig. 12, wherein the transformer winding are designated by the same numerals as previously and the magnetic shunts are designated as 140 and 142. This decoupling by the inductance permits the vectors representing the voltages of winding 112 and at winding 78 to be independently adjusted.

Such types of systems, their backgrounds and the theory of their operation are described, for example in G. J. Smollinger and W. J. Raddi, "Reverse Energy Through an A.C. Line Synchronized Pulse Width Modulated Sine-Wave Inverter", Intelec 81, pp. 126-131; R. Rando, "AC Triport - A New Uninterruptible AC Power Supply", Intelec 78, pp. 50-581; G.E. Neajsm "A Stored-Program Controlled Triport UPS", Intelec 81, pp. 210-215; and Z. Noworolski and K. Goszyk, "High Efficiency Uninterruptible Power Supply", 4th International PCI Conference on Power Conversion, March, 1982, pp. 521-529.

In the embodiment of Fig. 11, the connection between the high utility line 96 and winding 76 includes a series fuse 150 and an AC disconnect switch 122, similar in form to the static bypass switch means 120 and AC switch means 60, that are similarly operable, when desired, by electrical signals applied by switch control means 150 to the

gate electrodes of the SCR's. For example, when the utility line fails, switch 122 is automatically opened and the load is supplied with AC power entirely from the battery and inverter.

5 In this embodiment of the invention, the ratio R of the number of turns N_2 of transformer winding 80 to the number of turns N_1 of transformer winding 76 is other than unity, i.e., $N_2/N_1 = 1.1$. The significance of this will now be described with
10 respect to Figs. 8, 13 and 14, especially.

 The simplified equivalent circuit illustrated in Fig. 8 is applicable to the system of Fig. 11, the ratio N_2/N_1 of the turns of the windings 80 and 76 being represented by the tap position on an auto
15 transformer which, in effect, increases the line voltage applied to the input end of inductance L_S from E_U to a 10% higher value E_U' . The series inductance L_S is effectively provided, in the example of Fig. 11, by the transformer 84 and the magne-
20 tic shunts 114, 116 built into it. As described previously with respect to Figs. 7 and 9, this step-up ratio of 1.1 minimizes the break-even inverter current required by the system during normal operation and maximizes the through-put
25 efficiency.

 The transformer 84 in this example is of EI construction, with the magnetic shunts described previously serving to attenuate the magnetic path between winding 76 and windings 112, 78 and 80, in
30 this example giving an effective value for L_S of about 5 millihenries.

Figs. 13A and 13B illustrate from a different viewpoint the operation and effect of the line voltage step-up employed. Fig. 13A illustrates the phase relationships in a typical prior-art apparatus in which $E_U = E_i$ and E_i lags E_U (for example, by 23° in a typical operating condition). The difference vector E_L again represents the voltage across the series inductance L_S , and the current through that inductance is represented by the vector I_L at the right angles thereto. The output current in this example is assumed to be in phase with the inverter output voltage (ie the load is unity power factor) so that the I_O vector lies along the same direction as the E_i vector as shown. The difference vector I_i then represents the substantial circulating current in the inverter, which always exists under these conditions even though no real power is then being delivered to or from the inverter.

Fig. 13B shows conditions existing in a comparable system modified in accordance to the present invention so that the line voltage E_U is, in effect, transformed upwardly by a factor 1.1 to a new value E_U' , this increased value of E_U' being sufficient so that the E_L vector is vertical and the I_L vector, being at right angles to E_L , lies directly along the direction of the inverter current I_O and is equal thereto. It therefore supplies all of the load current, leaving no current, reactive or real, in or out of the inverter, as is desired to

produce the previously-described improvements with regard to minimizing inverter current and improved through-put efficiency.

It can be seen from Figs. 13A and 13B that
5 varying the length of E_U' exerts an action as if the E_L and I_L vectors were fixed at right angles to each other but rotatable together about the end of the E_i vector so that, by appropriate selection of the
10 length of E_U' , I_L can be turned into alignment with I_O regardless of the direction of I_O , which direction may vary depending upon the load factor, for example.

Fig. 14 illustrates by way of example one type
of system in which the UPS of the present invention
15 may be included. In this case a microprocessor 300, such as a 280 microprocessor chip, controls the frequency and phase β of the inverter output
sinewave is supplied with appropriate program memory
information from memory 302; with system personality
20 information indicative of the particular application parameters from system personality 304; with digital information with respect to line voltage, load
voltage, line current, load current, battery current
and battery voltage from A/D device 308; with a
25 variety of monitoring information with respect to conditions of the line switch, the bypass switch, over-temperature, over-voltage or any other
parameters which it is desired to monitor, by way of
I/O port 310; and with a mutual interchange of
30 information with an appropriate display device 312.

The microprocessor also preferably receives information from an interrupt control 310 with respect to such parameters as line voltage, inverter voltage, time and any other parameters found desirable. In this example, the microprocessor controls a counter timer chip (CTC) carrier generator 400 and a CTC 60Hz generator 402, which operate to produce on line 404 a carrier frequency equal to the repetition rate of the pulse-width modulated pulses (typically at 26 times the 60 Hertz line frequency) and to produce from sine generator 410 a substantially pure sinewave function at utility-line frequency and of the desired 120-volt magnitude. The PWM control 420 controls the inverter 422, which in this case is assumed to be the entire circuit of Fig. 11, so as to determine the phase and the widths of the pulses which turn on the transistors in the PWM bridge circuit. An inverter feedback connection extends from the load 450 to a comparison or error amplifier circuit 452 which detects and amplifies any differences between the voltage fed back from the inverter and the idealized sinewave from sine generator 410, this difference then being fed to PWM control 420 in a polarity and amount to correct any deficiencies in the sinewave appearing at the load. Normally the sinewave is locked to the utility line sinewave. However, to provide a suitable sinewave to the comparison circuit upon a utility line outage, the

microprocessor includes a stable crystal-controlled reference oscillator, powered by the battery, from which the desired ideal sinewave at the desired line frequency is derived.

5 The microprocessor maintains frequency lock between the sinewave reference and the utility as well as manipulating the displacement phase angle between them. It also examines all system parameters and compares them against preset software
10 limits. The user can access these system parameters through a front graphics display panel.

 Figs. 15A and 15B illustrate the bidirectional line conditioning obtained with the isolated system of the present invention. As shown in Fig. 15A, if
15 the line voltage E_U consists of a sinewave with the noise spikes shown thereon, the inverter voltage E_i supplied to the load has the substantially pure sinewave appearance shown in the latter figure; Fig. 15B shows that even if the load current I_O were
20 distorted as shown, this would not reflect back into, or substantially distort, the utility supply line current I_U , which remains a substantially pure sinewave.

 The preferred embodiment of the invention has
25 been shown as utilizing a transformer in which magnetic shunts provide the effective series inductance L_S , and the voltage step-up R is provided by the ratio N_2/N_1 in the number of turns of entirely separate and isolated transformer windings. How-
30 ever, many of the advantages of the invention with

regard to minimizing inverter current and maximizing through-put can be obtained where the series inductance L_s is in fact a real lumped-circuit series inductor connected between the high side of the line and the inverter output, much as represented schematically in the simplified equivalent circuit of Fig. 8, and it is in fact possible to utilize an auto transformer as suggested by the equivalent circuit of Fig. 8 rather than the completely isolated transformer winding arrangement of the preferred embodiment.

Also, although the ratio of E_u'/E_u of 1.1 has been found preferable for many practical purposes, the minimum inverter current may in some instances occur at a different value than 1.1, in which case R may be differently chosen to minimize inverter current during break-even operation. That is, in some cases the load power factor may not be centered about unity, but may have a known average fixed value departing substantially from unity, in which case the value of R may be chosen to be substantially different from 1.1, so as to minimize the required inverter current during normal operation.

TABLE 1

$E_U = 1.0$ L_s		Load PF = 1		Load PF = 0.8 lag		Load PF = 0.9 load	
		Breakeven Charge	Breakeven Charge	Breakeven Charge	Breakeven Charge	Breakeven Charge	Breakeven Charge
0.2 P.U.	I_i	0.19	0.39	0.77	0.87	0.34	0.49
-	β	13°	15.5°	12°	14°	12°	15.5°
0.4 P.U.	I_i	0.31	0.55	0.86	1.01	0.25	0.36
	β	27°	33°	24°	29°	25°	30°
0.6 P.U.	I_i	0.53	0.87	1.04	1.12	0.17	0.41
	β	45°	57°	40°	48°	40°	50°
$E_U = 0.85 (-15\%)$							
0.2 P.U.	I_i	0.99	1.12	1.55	1.66	1.51	0.67
	β	17°	20°	15°	18°	15°	18°
0.4 P.U.	I_i	0.77	1.02	1.29	1.46	0.25	0.49
	β	34°	42°	30°	36°	29°	36°
0.6 P.U.	I_i	0.99	1.61	1.39	1.75	0.37	0.74
	β	60°	65°	50°	65°	50°	65°

TABLE 2

$E_U = 1.1$ L_s		Load PF = 1		Load PF = 0.8 lag		Load PF = 0.9 load	
		Breakeven	Charge	Breakeven	Charge	Breakeven	Charge
0.4 P.U.	I_i	0.12	0.35	0.58	0.72	0.49	0.51
	β	24°	29°	21°	25°	23°	27°
	γ	24°	24°	25°	25°	25°	24°
$E_U = 0.935 (-15\%)$							
0.4 P.U.	I_i	0.52	0.72	1.03	1.21	0.12	0.35
	β	30°	36°	26°	32°	26°	32°
	γ	7°	11°	4°	8°	4°	8°

(42)



CLAIMS:

1. A stabilized power supply for supplying
alternating current power to a critical load, such
as a computer, comprising transformer means including
an output winding connected with the load, and first,
5 second and third input windings, first supply means
including a battery and an inverter for supplying
alternating-current power, second supply means for
supplying alternating-current power, transfer switch
means having first and second conditions for alternating
10 connecting and disconnecting said first supply means
and said first input winding for the supply of power to
the load and for disconnecting and connecting said
second supply means and said second input winding
for the supply of power to the load, respectively,
15 means connecting said third input winding with a third
power supply means, and means affecting the vector
relationship between the voltages of said third and
first supply means to cause the real component of the
inverter current at the break-even condition to be a
20 minimum.

2. A power supply as claimed in claim 1, wherein
said means affecting the vector relationship comprises
magnetic shunt means for ^{affecting} ~~varying~~ the coupling between
the windings of said transformer means, said magnetic
25 shunt means being arranged at least partially to
isolate said third winding from said first and second
windings.

3. A power supply as claimed in claim 1 or
claim 2, wherein said means affecting the vector
30 relationship comprises an inductance.

4. A power supply as claimed in any preceding
claim, further including means for stepping up the
voltage of said third supply means relative to that
of said first supply means, thereby to minimize
35 the break-even inverter current required by the
system during normal operation, and to maximise the
through-put efficiency.

5. A power supply as claimed in claim 4, wherein said voltage step-up means includes an auto-transformer.

5 6. A power supply as claimed in claim 4, wherein the number of turns of said output winding is greater than that of said third input winding to produce the desired step-up voltage.

10 7. A power supply as claimed in claim 1, and further including means operable by said transfer switch means for connecting between said inverter and said first winding a dummy inductance so dimensioned as to correspond with the inductance that is produced when the ~~third~~ supply means is connected with said third winding, thereby to permit the inverter to recharge
15 the battery even when the load is connected with the ^{second} supply means.

8. A power supply as claimed in claim 7, wherein said inverter comprises a four-quadrant pulse-width-modulated sinewave inverter.

20 9. A power supply as claimed in claim 8, wherein said transfer switch means includes for each input winding a pair of oppositely poled controlled-diode rectifiers connected in parallel, and switch control means for operating said diodes in response
25 to system malfunction.

10. A power supply as claimed in claim 1 and substantially as hereinbefore described with reference to, and as shown in, the accompanying drawings.

