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MULTIPLE CARRIER DIGITAL TELEVISION SIGNAL DECODER

5 This invention concerns a digital television decoding apparatus, for use in for example a high definition television (HDTV) system, which is responsive to a multiple carrier modulation signal, such as a pulse amplitude modulation (PAM) signal. One of various forms of PAM is quadrature amplitude
10 modulation (QAM) which will be used to describe an embodiment of the invention. A prioritized dual carrier QAM decoding system is described in U.S. Patent 5,287,180 - H.E. White, and in U.S. Patent 5,122,875 - Raychaudhuri et al.

 In a QAM symbol transmission system, a transmitted data
15 symbol is represented by both "I" and "Q" quadrature components which modulate respective quadrature phased carriers at a given frequency. Each symbol may comprise several bits, and the number of bits/symbol dictates the type of QAM system, i.e., 16-QAM, 32-QAM, etc. Each symbol is mapped (assigned) to a
20 prescribed coordinate in a four-quadrant grid-like constellation using a look-up table (e.g., a ROM). A prescribed number of symbols occupy assigned areas in each quadrant. In a 32-QAM system, each quadrant of the constellation contains eight symbols at prescribed coordinates with respect to quadrature I and Q axes.
25 Certain symbol bits designate the constellation quadrant in which a symbol is located, and certain bits designate the particular coordinate in that quadrant assigned to the symbol. QAM systems of this general type are well known.

 In the system disclosed in White and in Raychaudhuri et al.,
30 a television signal representing high definition image information is transmitted using two QAM carriers frequency multiplexed in a standard 6 MHz television transmission baseband. One of the carriers conveys high priority information, while the other carrier conveys (relatively lower) standard priority information. The
35 high priority (HP) information is the information needed to create a viewable image, although less than a perfect image, and is



conveyed with significantly more power than the standard priority (SP) information, which is the remaining information. The high priority information exhibits a narrow bandwidth compared to the standard priority information, and is therefore much less
5 prone to corruption by the transmission channel. The HP carrier is located in that portion of the frequency spectrum of a television transmission channel, e.g., an NTSC channel, which is normally occupied by the vestigial sideband of a standard NTSC television signal. This portion of the signal is normally significantly
10 attenuated by the Nyquist filters of standard receivers, so that HDTV signals with this transmission format will not introduce co-channel interference.

One approach to decoding such a dual QAM signal, as disclosed by White, employs two parallel signal paths for
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20 paths of White represent large, complex and expensive hardware components.

A system for reducing the amount of such parallel hardware to produce a less expensive system is described in U.S. Patent 5,263,108 - Lauren A. Christopher, "Apparatus for Time Division
25 Multiplexed Processing of Plural QAM Signals". To this end the Christopher system employs time division multiplexed processing of high priority and standard priority components of a received composite signal. While advantageously reducing the hardware requirements compared to the White system, the system
30 described by Christopher introduces the added complication of time division multiplexing. The signal processing system described herein offers a further refinement of a prioritized QAM decoder by advantageously avoiding both the hardware requirements of White and the time division multiplex complexity
35 exhibited by Christopher, without compromising the quality of a decoded QAM signal.



In accordance with the principles of the invention there is provided digital signal processing apparatus for processing a television signal, and having input means for receiving a multiple carrier composite PAM signal. Signal conditioning means, including adaptive equalizer means, is responsive to the composite signal for providing a conditioned composite signal at an output. The equalizer means includes a single equalizing device having a wideband response encompassing more than one of the carriers and defined by one set of coefficients for equalizing the more than one carriers without separating the carriers from the spectrum of said composite signal prior to equalization. There is also provided means for deriving an error signal representing a condition of said PAM signal, and means for coupling the error signal to the signal conditioning means.

15

Brief Description of the Drawing

FIGURE 1 is a block diagram of a digital HDTV QAM receiver/decoder in accordance with the principles of the present invention.

FIGURE 2 depicts the baseband video frequency spectrum of a dual QAM high definition television signal received by the system of FIGURE 1.

25

Detailed Description

Before discussing the system shown in FIGURE 1, it will be helpful to consider FIGURE 2, which depicts the frequency spectrum of a prioritized dual 32-QAM baseband video signal produced by the disclosed system as will be discussed.

FIGURE 2 illustrates the video frequency spectrum of a high definition television signal which is compatible with the 6 MHz bandwidth of a standard NTSC television signal channel, and which can be used as a simulcast signal. To facilitate comparison with a standard NTSC video frequency spectrum, the frequencies along the frequency scale of FIGURE 2 (-1.25 MHz to 4.5 MHz) are



referenced to the 0.0 MHz frequency location of the RF picture carrier in an NTSC system.

The HDTV signal is a data compressed signal divided, for example, into high and standard priority components. In this example audio, synchronizing and low frequency video information components which are intended to be received with high reliability are assigned a high priority. The synchronizing information, for example, may be in the nature of a training signal containing a unique signature or code to facilitate signal recovery and processing at a receiver, and illustratively may include field rate scanning information (e.g., start of field markers). Other less critical components, such as high frequency video information, are assigned a lower standard priority. The high priority information exhibits a narrow bandwidth relative to the standard priority information, and quadrature amplitude modulates (QAM) a 0.96 MHz first suppressed carrier referenced to a carrier reference signal REF as discussed below. The standard priority information quadrature amplitude modulates a 3.84 MHz second suppressed carrier which is also referenced to signal REF. A resulting composite signal is a form of a multiple QAM signal, i.e., a "dual" QAM signal in this instance. The composite dual QAM signal is translated into the 6 MHz standard television band by means of out-of-band reference signal REF. The frequency of signal REF is chosen so that when signal REF is modulated by the composite QAM signal, one of the resulting sum or difference components falls within the band of frequencies associated with a desired radio frequency television channel, such as simulcast VHF channel 3. Signal REF is modulated by the composite dual QAM signal to produce a double sideband modulated signal, the lower sideband of which is rejected and the upper sideband of which is retained as illustrated by FIGURE 2.

The amplitude of the narrowband HP QAM component is significantly greater than that of the wideband SP component, e.g., twice as large. The -6db bandwidth of the HP component is 0.96 MHz, and the -6db bandwidth of the SP component is 3.84 MHz, which is four times the bandwidth of the HP component. The



band edge transition regions of the narrowband HP and wideband SP components are shaped by finite impulse response (FIR) filters with a square root of a raised cosine characteristic, to produce smooth transition regions which avoid unwanted high frequency effects produced by sharp transition regions.

The HP and SP QAM signals each contain quadrature "I" and "Q" components. A data word, or symbol, is represented by both I and Q components. In the case of a 32-QAM signal, each I and Q component exhibits eight discrete amplitude levels, resulting in a total of 32 possible amplitude levels, or values (8 levels x 4 quadrants), for each HP and SP QAM signal. Three bits are needed to specify the eight levels of each I and Q component, and two bits specify the QAM constellation quadrant. Thus each symbol requires five bits to specify the thirty-two coordinates of a four quadrant 32-QAM constellation.

The 32-QAM signal to be discussed exhibits symbol rates of 0.96 MHz and 3.84 for the HP and SP data, respectively. The symbol rate is independent of the type of QAM processing being used (e.g., 16-QAM or 32-QAM). Using four time oversampling, the HP sampling rate is 3.84 MHz and the SP sampling rate is 15.36 MHz. At five bits per symbol in the case of 32-QAM, the HP and SP bit rates are 4.8 Mbps and 19.2 Mbps, respectively.

The described prioritized dual QAM system exhibits significant co-channel immunity from interference associated with a standard NTSC television signal, i.e., an NTSC signal transmitted from a different location in the same channel as the dual QAM signal. This is due to attenuating notches in the QAM spectrum in the vicinity of the NTSC RF picture carrier and the NTSC sound carrier, which are associated with high energy information. Conversely, co-channel interference from the dual QAM signal into an NTSC signal is significantly reduced because the large amplitude narrowband QAM signal will be significantly attenuated by a Nyquist slope filter in a standard NTSC television receiver. In FIGURE 2 the Nyquist slope filter response in a standard NTSC receiver is indicated by a dotted line superimposed on the low band portion of the QAM spectrum from -0.75 MHz to 0.75 MHz.



The combination of the 6dB greater amplitude of the narrowband QAM component and its one-quarter bandwidth relative to the wideband QAM component results in a significantly greater power density than that of the wideband QAM component. The
5 illustrated high priority narrowband QAM signal therefore exhibits a significant signal-to-noise improvement and lower error rate relative to the low priority wideband QAM signal.

The large peak amplitude narrowband component contains video information sufficient to produce a displayed image with
10 definition approximating that of a standard definition television image. Thus a viewer should not be overly disturbed if, for example, the high definition transmission is momentarily disrupted. If the low power wideband component containing the high definition information is disrupted momentarily, the high
15 power narrowband component may be unaffected whereby a lower definition but acceptable image is displayed momentarily.

The invention will be described in the context of an Advanced Definition Television (ADTV) receiver system of the type for processing HDTV signals proposed by the Advanced
20 Television Research Consortium (ATRC). The television signal represented by the spectrum shown in FIGURE 2 is such a proposed HDTV signal. However, the practice of the invention is not limited to use in such a system.

FIGURE 1 illustrates a portion of an ADTV receiver
25 incorporating apparatus according to the present invention. A broadcast television signal having the spectral characteristics illustrated in FIGURE 2 is applied to an input unit 10 including tuner and Intermediate Frequency (IF) network. A local oscillator in the IF network down converts the center of the SP channel to
30 the symbol rate of the SP channel (3.84 MHz), whereby the center of the HP channel is down-converted to the symbol rate of the HP channel (0.96 MHz). The IF frequency is 43.5 MHz in this example, which places the center of the baseband SP channel at 3.84 MHz. The down converted signal is converted from analog to
35 digital form by an analog-to-digital converter 12. Converter 12 is



clocked at 15.36 MHz, which is four times the symbol rate of the SP data.

Timing reference generator 16 includes band-edge timing recovery circuits for developing a symbol rate clock from the HP or SP spectrum of the QAM signal provided to unit 16 from the output of A/D converter 12. Unit 14 may include a voltage controlled crystal oscillator incorporated in a phase locked loop for deriving a 15.36 MHz sampling clock for A/D converter 12 in response a symbol rate output signal from reference generator 16.

10 The symbol rate output signal from unit 16 synchronizes the oscillator in unit 14. Clock recovery unit 14 also develops other clock signals CLK1 ... CLKN for application to other units of the system as needed. Additional details of clock recovery networks to recover a symbol rate clock from a QAM signal are found in the

15 reference text Digital Communications by Lee and Messerschmitt (Klewer Academic Press, Boston, MA, USA, 1988).

The composite digital QAM signal, including HP and SP components each with I, Q quadrature components, is applied to a 90° phase shifting network 18 which separates the I and Q

20 components. The HP and SP "I" component appears at the I output of unit 18, and the HP and SP "Q" component appears at the Q output of unit 18. Unit 18 may employ a 90° Hilbert phase shifter, as is known, to provide the separated quadrature I and Q components, or a pair of multipliers (mixers) which respond to the

25 output signal from unit 12 and to respective sine and cosine reference signals.

The HP, SP I signal and the HP, SP Q signal from unit 18 are applied to a signal conditioning network including a complex digital adaptive (FIR) equalizer 20 which compensates for

30 transmission channel perturbations, and a QAM constellation de-rotator 24. Equalizer 20 is a single wideband equalizer with a response defined by one set of coefficients, and having one set of multipliers, and responds to dynamically updated filter coefficients from a unit 22 as will be discussed. Adaptive

35 equalization is discussed in detail in the Lee and Messerschmitt text mentioned previously. De-rotator 24 compensates for a



dynamic phase error manifested by a slight rotation of the received QAM constellation. This error may be produced by a variety of factors including local oscillator frequency variations, for example. The constellation phase error/rotation may be
 5 significantly reduced or eliminated by a so-called carrier recovery network. In this example the carrier recovery network includes de-rotator 24 which responds to equalized I and Q signals from unit 20, a phase control unit 26, a slicer 28, and an error detector 30 which develops an error signal E1 for use by phase control unit
 10 26. Units 24, 28, 30 and 26 comprise the essential elements of a digital phase locked loop for eliminating the dynamically varying QAM constellation offset. A filter 32 and a baseband demodulator 25 are included in the phase locked loop.

More specifically, the composite QAM signal is separated
 15 into its High Priority (HP) and Standard Priority (SP) components by means of a real coefficient digital low pass filter 32 and a real coefficient digital band pass filter 34, respectively. More expensive complex coefficient filters also could be used. The following description of the processing of the HP component from
 20 filter 32 via units 25, 28, 30 and 40 also applies to the processing of the SP component from filter 34 via corresponding units 27, 36, 38 and 42.

The high priority I and Q components from filter 32 are demodulated to baseband by means of demodulator 25, which
 25 may exhibit one of several known forms. For example, demodulator 25 may comprise a time demultiplexer and inverter to perform the demodulation mixing process. For additional information about digital QAM modulation and demodulation, see VLSI Architecture for a High-Speed All-Digital Quadrature
 30 Modulator and Demodulator for Digital Radio Applications, H. Samuelli, IEEE Journal on Selected Areas in Communications, Vol. 8, No. 8, Oct. 1990.

Slicer 28 contains a mapping mechanism and is programmed to select the constellation symbol closest in distance to the
 35 received signal sample. The complex I, Q plane (constellation) is divided into decision regions where each decision region is the set



of points that is closest to some symbol. If, after examining a decision region for a symbol, a received symbol is found to be located at or offset in distance from an expected coordinate, slicer 28 produces an output symbol at the expected coordinate. The slicer output symbol differs from the slicer input symbol by the amount of any distance offset. The amount of any such offset is sensed by error detector 30, which produces an output error signal E1 as a function of the amount of offset. Output error signal E1 may be produced by a complex multiplier associated with error detector 30.

The error signal from detector 30 is provided to phase control unit 26 for generating quadrature sine and cosine correction coefficients. These correction coefficients, and the I, Q components from equalizer 20, are provided to multipliers associated with de-rotator 24 for performing the de-rotating function. It can be shown that any set of quadrature signals can be rotated to a desired angular position by performing a complex multiplication on the quadrature signals. That is, quadrature signals I and Q can be rotated to conform to corrected quadrature signals I' and Q' according to the expressions:

$$I' = I \cos (f) + Q \sin (f)$$

$$Q' = Q \cos (f) - I \sin (f)$$

where (f) is an error correction angle produced as a function of error signal E1 in this example. A more detailed discussion of a carrier recovery network including this type of de-rotator apparatus is found in the Lee and Messerschmitt text noted previously.

Only one error signal, E1 in this example, is needed to dynamically restore (de-rotate) the QAM constellation to a correct orientation, since an error signal derived from either the HP component or the SP component would represent substantially the same carrier frequency or phase error, and would produce the same control effect.

Error signal E1 also is applied to a control input of coefficient control network 22 associated with equalizer 20. Another control input of network 22 receives an error signal E2 generated by



slicer 36 and error detector 38 in the standard priority component processor. Standard priority error signal E2 is generated in the same manner as previously discussed high priority error signal E1. Unit 22 is a digital signal processor responsive to a prescribed
5 algorithm for providing updated equalizer filter coefficients as a function of error signals E1 and E2. The algorithm used by network 22 may vary, depending on the requirements of a particular system. For example, updated coefficients may be generated simply as a result of combining error signals E1 and E2,
10 and may operate so as to minimize error signals E1 and E2 substantially simultaneously. The updated coefficients generated by network 22 are applied to a coefficient Random Access Memory (RAM) associated with digital adaptive FIR equalizer 20.

An adaptive equalizer such as unit 20 is a complex,
15 hardware intensive device even when, as in this embodiment, it is not subjected to time multiplexed operation at a high switching rate. Equalizer 20 is considerably more complex than other signal processing units including units 24, 25, 26, 28, 30, 32 and 40. Equalizer 20 may be of a conventional design with an adaptive
20 digital FIR filter network to compensate for amplitude and frequency/phase irregularities caused by the transmission channel. In this example equalizer 20 is a decision directed passband equalizer responsive to dynamically updated coefficients provided by network 22 in response to feedback error
25 signals E1 and E2. The equalizer coefficients are dynamically updated by signals E1 and E2 after an initialization interval during which equalizer 22 is initialized using blind equalization or using training signal techniques. Equalizer 20 preferably is a fractionally spaced device which exhibits an adaption rate which
30 is a fraction of the symbol rate.

Processed high priority components HP-I and HP-Q from unit 28, and processed standard priority components SP-I and SP-Q from unit 36, are respectively decoded by units 40 and 42 to recreate the original bitstreams. Units 40 and 42 include a
35 differential decoder to perform the inverse of the differential symbol coding and mapping operations performed by the



transmitter encoder for both HP and SP data. Look-up tables are used to un-map the four quadrant signal constellations into the original sequential five-bit symbol segments which existed at the transmitter before being differentially encoded and QAM

5 modulated as is shown.

Recovered HP symbol data from decoder 40 and recovered SP symbol data from unit 42 are applied to respective inputs of an audio/video signal processing and reproducing unit 48. Unit 48 may include data decompression networks such as

10 Huffman decoders and inverse quantizers, error correcting networks, and de-multiplexing networks for providing separate audio and video television signal components. These components may be reproduced by suitable sound reproduction or video display means. Alternatively, these components may be stored by

15 magnetic or optical storage media.

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CLAIMS

1. In a system for processing a television signal,
digital signal processing apparatus wherein:
5 input means (10) for receiving a multiple carrier
composite PAM signal;
signal conditioning means (25,27,28,36,40,42),
including adaptive equalizer means (20), responsive to said
composite signal for providing a conditioned composite signal at
10 an output, said equalizer means including a single equalizing
device having a wideband response encompassing more than one
of said carriers and defined by one set of coefficients for
equalizing said more than one carriers without separating said
more than one carriers from the spectrum of said composite signal
15 prior to equalization;
means (30,38) for deriving an error signal
representing a condition of said PAM signal; and
means (22) for coupling said error signal to said signal
conditioning means.
20
2. Apparatus according to claim 1, wherein
said multiple carrier composite signal comprises a first
carrier modulated by a first information component and a second
carrier modulated by a second information component;
25 said deriving means includes means for separating
said first information component and said second information
component of said conditioned composite signal, and detector
means responsive to a separated component from said sensing
means for developing said error signal; and wherein said
30 apparatus further includes
means for combining said separated first and second
components.

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3. Apparatus according to claim 1, wherein
said equalizer means exhibits non-time-multiplexed
operation.

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4. Apparatus according to claim 2, wherein
said composite signal is a digital high definition
television signal and said first and second components are
frequency multiplexed in a baseband spectrum.

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5. Apparatus according to claim 4, wherein
said first and second components exhibit different
carrier frequencies and different bandwidths occupying different
portions of a television signal video spectrum.

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6. Apparatus according to claim 2, wherein said signal
conditioning means further includes
de-rotator means responsive to an equalized
composite signal from said equalizer means, and to an error signal
20 developed by said detector means for maintaining a desired
orientation of said constellation.

7. Apparatus according to claim 6, wherein
said detector means derives first and second error
25 signals from said separated first and second components,
respectively;

said equalizer means is responsive to said first and
second error signals; and

said de-rotator means is responsive to one of said
30 error signals.

8. Apparatus according to claim 2 and further
comprising

means for differentially decoding said first component
35 and said second component prior to being combined by said
combining means.



9. Apparatus according to claim 4, wherein
said baseband spectrum is constituted by a first
frequency band occupying the lowermost portion of said
5 spectrum, and a second frequency band occupying the remainder
of said spectrum, said first band being narrower than said second
band, exhibiting higher energy than said second band, and
containing higher priority information than said second band.
10. Apparatus according to claim 9, wherein
said first band contains low frequency video
information and audio information; and
said second band contains high frequency video
information occupying frequencies including standard
15 chrominance frequencies and a standard chrominance subcarrier
frequency.
11. Apparatus according to claim 1, wherein
said adaptive equalizer means is a fractionally spaced
20 passband equalizer.
12. In a system for processing a television signal,
digital signal processing apparatus wherein:
input means (10) for receiving a composite multiple
25 carrier PAM signal, said multiple carrier composite signal
comprising a first carrier modulated by a first component, and a
second carrier modulated by a second component;
signal conditioning means (18-26) including adaptive
equalizer means (20) exhibiting non-time-multiplexed operation
30 and responsive to said composite signal for providing an equalized
composite signal at an output, said equalizer means including a
single equalizing device having a response encompassing said first
and second modulated carriers for equalizing said first and second
modulated carriers without separating said first and second
35 modulated carriers from the spectrum of said composite signal
prior to equalization;





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means (32,34) for separating said first component and said second component of a conditioned composite signal from said conditioning means;

5 first means (28,40) responsive to separated data associated with said first component for producing corresponding output data;

first detector means (30) for producing a first error signal (E1) representing an offset between respectively corresponding input and output data of said first means;

10 second means (36,42) responsive to separated data associated with said second component for producing corresponding output data;

second detector means (38) for producing a second error signal (E2) representing an offset between respectively
15 corresponding input and output data of said second means;
wherein

said adaptive equalizer means (20) is responsive to said first and second error signals.

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Abstract of the Disclosure

In a video signal processing system, a single adaptive passband equalizer (20) is used to process a composite Quadrature Amplitude Modulated (QAM) signal encoded with high priority (HP) and standard priority (SP) components. The equalizer output is phase corrected by a de-rotator(24), and filtered (32,34) to separate the HP and SP components. Error signals respectively representing HP and SP phase errors are developed (30,38). One of the error signals (E1) controls the operation of the de-rotator. Both error signals are used to generate (22) updated coefficients for the adaptive equalizer. Afterwards the HP and SP components are decoded (40,42) and combined (48).

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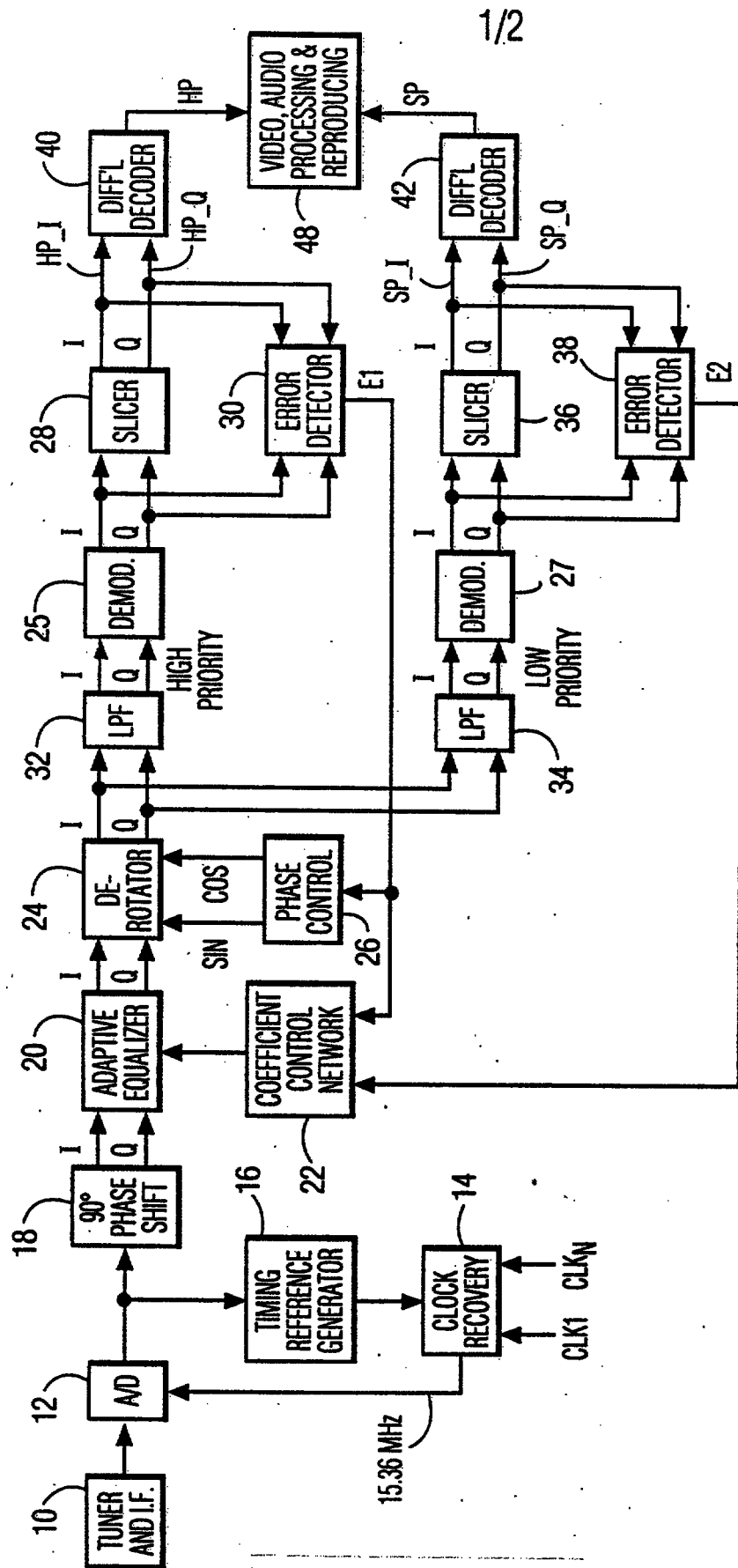


FIG. 1



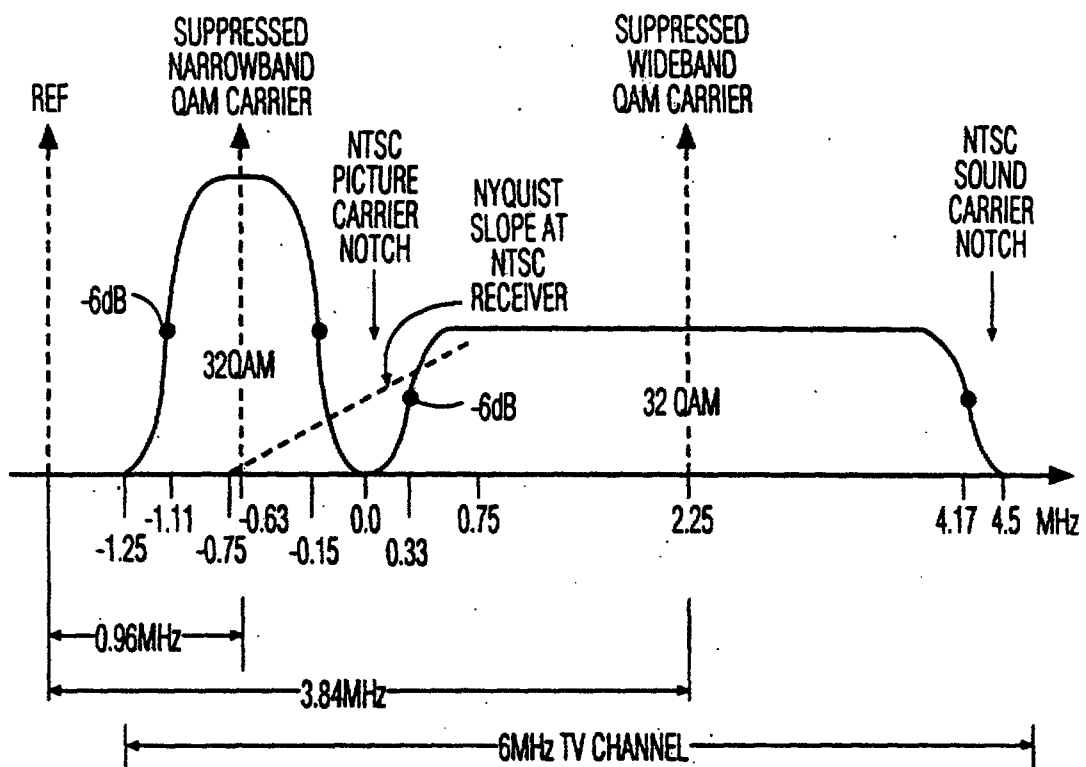


FIG. 2

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TELEVISION SIGNAL DECODER**

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10 attenuated by the Nyquist filters of standard receivers, so that HDTV signals with this transmission format will not introduce co-channel interference.

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Brief Description of the Drawing

FIGURE 1 is a block diagram of a digital HDTV QAM receiver/decoder in accordance with the principles of the present
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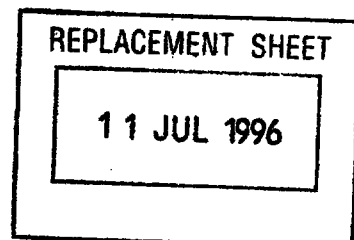
FIGURE 2 depicts the baseband video frequency spectrum of a dual QAM high definition television signal received by the system of FIGURE 1.

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The amplitude of the narrowband HP QAM component is significantly greater than that of the wideband SP component, e.g., twice as large. The -6db bandwidth of the HP component is 0.96 MHz, and the -6db bandwidth of the SP component is 3.84 MHz, which is four times the bandwidth of the HP component. The

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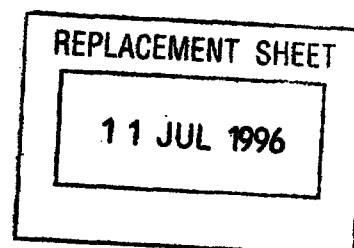
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band edge transition regions of the narrowband HP and wideband SP components are shaped by finite impulse response (FIR) filters with a square root of a raised cosine characteristic, to produce smooth transition regions which avoid unwanted high frequency effects produced by sharp transition regions.

The HP and SP QAM signals each contain quadrature "I" and "Q" components. A data word, or symbol, is represented by both I and Q components. In the case of a 32-QAM signal, each I and Q component exhibits eight discrete amplitude levels, resulting in a total of 32 possible amplitude levels, or values (8 levels x 4 quadrants), for each HP and SP QAM signal. Three bits are needed to specify the eight levels of each I and Q component, and two bits specify the QAM constellation quadrant. Thus each symbol requires five bits to specify the thirty-two coordinates of a four quadrant 32-QAM constellation.

The 32-QAM signal to be discussed exhibits symbol rates of 0.96 MHz and 3.84 for the HP and SP data, respectively. The symbol rate is independent of the type of QAM processing being used (e.g., 16-QAM or 32-QAM). Using four time oversampling, the HP sampling rate is 3.84 MHz and the SP sampling rate is 15.36 MHz. At five bits per symbol in the case of 32-QAM, the HP and SP bit rates are 4.8 Mbps and 19.2 Mbps, respectively.

The described prioritized dual QAM system exhibits significant co-channel immunity from interference associated with a standard NTSC television signal, i.e., an NTSC signal transmitted from a different location in the same channel as the dual QAM signal. This is due to attenuating notches in the QAM spectrum in the vicinity of the NTSC RF picture carrier and the NTSC sound carrier, which are associated with high energy information. Conversely, co-channel interference from the dual QAM signal into an NTSC signal is significantly reduced because the large amplitude narrowband QAM signal will be significantly attenuated by a Nyquist slope filter in a standard NTSC television receiver. In FIGURE 2 the Nyquist slope filter response in a standard NTSC receiver is indicated by a dotted line superimposed on the low band portion of the QAM spectrum from -0.75 MHz to 0.75 MHz.

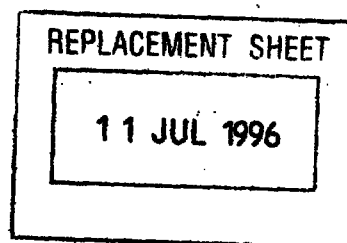


The combination of the 6dB greater amplitude of the narrowband QAM component and its one-quarter bandwidth relative to the wideband QAM component results in a significantly greater power density than that of the wideband QAM component. The
5 illustrated high priority narrowband QAM signal therefore exhibits a significant signal-to-noise improvement and lower error rate relative to the low priority wideband QAM signal.

The large peak amplitude narrowband component contains video information sufficient to produce a displayed image with
10 definition approximating that of a standard definition television image. Thus a viewer should not be overly disturbed if, for example, the high definition transmission is momentarily disrupted. If the low power wideband component containing the high definition information is disrupted momentarily, the high
15 power narrowband component may be unaffected whereby a lower definition but acceptable image is displayed momentarily.

The invention will be described in the context of an Advanced Definition Television (ADTV) receiver system of the type for processing HDTV signals proposed by the Advanced
20 Television Research Consortium (ATRC). The television signal represented by the spectrum shown in FIGURE 2 is such a proposed HDTV signal. However, the practice of the invention is not limited to use in such a system.

FIGURE 1 illustrates a portion of an ADTV receiver
25 incorporating apparatus according to the present invention. A broadcast television signal having the spectral characteristics illustrated in FIGURE 2 is applied to an input unit 10 including tuner and Intermediate Frequency (IF) network. A local oscillator in the IF network down converts the center of the SP channel to
30 the symbol rate of the SP channel (3.84 MHz), whereby the center of the HP channel is down-converted to the symbol rate of the HP channel (0.96 MHz). The IF frequency is 43.5 MHz in this example, which places the center of the baseband SP channel at 3.84 MHz. The down converted signal is converted from analog to
35 digital form by an analog-to-digital converter 12. Converter 12 is



clocked at 15.36 MHz, which is four times the symbol rate of the SP data.

Timing reference generator 16 includes band-edge timing recovery circuits for developing a symbol rate clock from the HP or SP spectrum of the QAM signal provided to unit 16 from the output of A/D converter 12. Unit 14 may include a voltage controlled crystal oscillator incorporated in a phase locked loop for deriving a 15.36 MHz sampling clock for A/D converter 12 in response a symbol rate output signal from reference generator 16.

10 The symbol rate output signal from unit 16 synchronizes the oscillator in unit 14. Clock recovery unit 14 also develops other clock signals CLK1 ... CLKN for application to other units of the system as needed. Additional details of clock recovery networks to recover a symbol rate clock from a QAM signal are found in the

15 reference text Digital Communications by Lee and Messerschmitt (Klewer Academic Press, Boston, MA, USA, 1988).

The composite digital QAM signal, including HP and SP components each with I, Q quadrature components, is applied to a 90° phase shifting network 18 which separates the I and Q

20 components. The HP and SP "I" component appears at the I output of unit 18, and the HP and SP "Q" component appears at the Q output of unit 18. Unit 18 may employ a 90° Hilbert phase shifter, as is known, to provide the separated quadrature I and Q components, or a pair of multipliers (mixers) which respond to the

25 output signal from unit 12 and to respective sine and cosine reference signals.

The HP, SP I signal and the HP, SP Q signal from unit 18 are applied to a signal conditioning network including a complex digital adaptive (FIR) equalizer 20 which compensates for

30 transmission channel perturbations, and a QAM constellation de-rotator 24. Equalizer 20 is a single wideband equalizer with a response defined by one set of coefficients, and having one set of multipliers, and responds to dynamically updated filter coefficients from a unit 22 as will be discussed. Adaptive

35 equalization is discussed in detail in the Lee and Messerschmitt text mentioned previously. De-rotator 24 compensates for a

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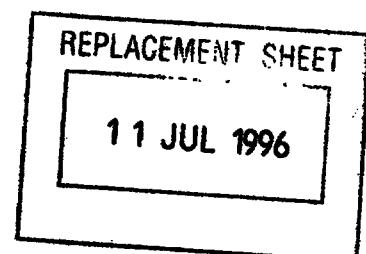
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dynamic phase error manifested by a slight rotation of the received QAM constellation. This error may be produced by a variety of factors including local oscillator frequency variations, for example. The constellation phase error/rotation may be significantly reduced or eliminated by a so-called carrier recovery network. In this example the carrier recovery network includes de-rotator 24 which responds to equalized I and Q signals from unit 20, a phase control unit 26, a slicer 28, and an error detector 30 which develops an error signal E1 for use by phase control unit 26. Units 24, 28, 30 and 26 comprise the essential elements of a digital phase locked loop for eliminating the dynamically varying QAM constellation offset. A filter 32 and a baseband demodulator 25 are included in the phase locked loop.

More specifically, the composite QAM signal is separated into its High Priority (HP) and Standard Priority (SP) components by means of a real coefficient digital low pass filter 32 and a real coefficient digital band pass filter 34, respectively. More expensive complex coefficient filters also could be used. The following description of the processing of the HP component from filter 32 via units 25, 28, 30 and 40 also applies to the processing of the SP component from filter 34 via corresponding units 27, 36, 38 and 42.

The high priority I and Q components from filter 32 are demodulated to baseband by means of demodulator 25, which may exhibit one of several known forms. For example, demodulator 25 may comprise a time demultiplexer and inverter to perform the demodulation mixing process. For additional information about digital QAM modulation and demodulation, see VLSI Architecture* for a High-Speed All-Digital Quadrature Modulator and Demodulator for Digital Radio Applications, H. Samueli, IEEE Journal on Selected Areas in Communications, Vol. 8, No. 8, Oct. 1990.

Slicer 28 contains a mapping mechanism and is programmed to select the constellation symbol closest in distance to the received signal sample. The complex I, Q plane (constellation) is divided into decision regions where each decision region is the set



of points that is closest to some symbol. If, after examining a decision region for a symbol, a received symbol is found to be located at or offset in distance from an expected coordinate, slicer 28 produces an output symbol at the expected coordinate. The slicer output symbol differs from the slicer input symbol by the amount of any distance offset. The amount of any such offset is sensed by error detector 30, which produces an output error signal E1 as a function of the amount of offset. Output error signal E1 may be produced by a complex multiplier associated with error detector 30.

The error signal from detector 30 is provided to phase control unit 26 for generating quadrature sine and cosine correction coefficients. These correction coefficients, and the I, Q components from equalizer 20, are provided to multipliers associated with de-rotator 24 for performing the de-rotating function. It can be shown that any set of quadrature signals can be rotated to a desired angular position by performing a complex multiplication on the quadrature signals. That is, quadrature signals I and Q can be rotated to conform to corrected quadrature signals I' and Q' according to the expressions:

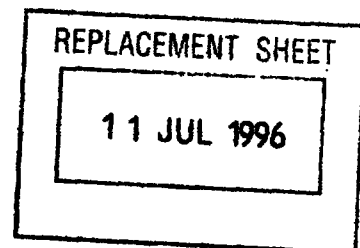
$$I' = I \cos (f) + Q \sin (f)$$

$$Q' = Q \cos (f) - I \sin (f)$$

where (f) is an error correction angle produced as a function of error signal E1 in this example. A more detailed discussion of a carrier recovery network including this type of de-rotator apparatus is found in the Lee and Messerschmitt text noted previously.

Only one error signal, E1 in this example, is needed to dynamically restore (de-rotate) the QAM constellation to a correct orientation, since an error signal derived from either the HP component or the SP component would represent substantially the same carrier frequency or phase error, and would produce the same control effect.

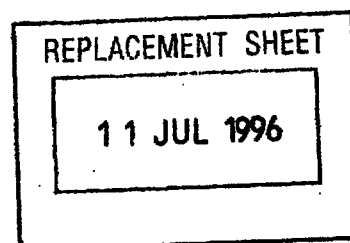
Error signal E1 also is applied to a control input of coefficient control network 22 associated with equalizer 20. Another control input of network 22 receives an error signal E2 generated by



slicer 36 and error detector 38 in the standard priority component processor. Standard priority error signal E2 is generated in the same manner as previously discussed high priority error signal E1. Unit 22 is a digital signal processor responsive to a prescribed
5 algorithm for providing updated equalizer filter coefficients as a function of error signals E1 and E2. The algorithm used by network 22 may vary, depending on the requirements of a particular system. For example, updated coefficients may be generated simply as a result of combining error signals E1 and E2,
10 and may operate so as to minimize error signals E1 and E2 substantially simultaneously. The updated coefficients generated by network 22 are applied to a coefficient Random Access Memory (RAM) associated with digital adaptive FIR equalizer 20.

An adaptive equalizer such as unit 20 is a complex,
15 hardware intensive device even when, as in this embodiment, it is not subjected to time multiplexed operation at a high switching rate. Equalizer 20 is considerably more complex than other signal processing units including units 24, 25, 26, 28, 30, 32 and 40. Equalizer 20 may be of a conventional design with an adaptive
20 digital FIR filter network to compensate for amplitude and frequency/phase irregularities caused by the transmission channel. In this example equalizer 20 is a decision directed passband equalizer responsive to dynamically updated coefficients provided by network 22 in response to feedback error
25 signals E1 and E2. The equalizer coefficients are dynamically updated by signals E1 and E2 after an initialization interval during which equalizer 22 is initialized using blind equalization or using training signal techniques. Equalizer 20 preferably is a fractionally spaced device which exhibits an adaption rate which
30 is a fraction of the symbol rate.

Processed high priority components HP-I and HP-Q from unit 28, and processed standard priority components SP-I and SP-Q from unit 36, are respectively decoded by units 40 and 42 to recreate the original bitstreams. Units 40 and 42 include a
35 differential decoder to perform the inverse of the differential symbol coding and mapping operations performed by the



transmitter encoder for both HP and SP data. Look-up tables are used to un-map the four quadrant signal constellations into the original sequential five-bit symbol segments which existed at the transmitter before being differentially encoded and QAM modulated as is shown.

Recovered HP symbol data from decoder 40 and recovered SP symbol data from unit 42 are applied to respective inputs of an audio/video signal processing and reproducing unit 48. Unit 48 may include data decompression networks such as Huffman decoders and inverse quantizers, error correcting networks, and de-multiplexing networks for providing separate audio and video television signal components. These components may be reproduced by suitable sound reproduction or video display means. Alternatively, these components may be stored by magnetic or optical storage media.

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1 2

CLAIMS

1. In a system for processing a television signal,
digital signal processing apparatus wherein:

5 input means (10) for receiving a multiple carrier
composite PAM signal;

 signal conditioning means (25,27,28,36,40,42),
including adaptive equalizer means (20), responsive to said
composite signal for providing a conditioned composite signal at
10 an output, said equalizer means including a single equalizing
device having a wideband response encompassing more than one
of said carriers and defined by one set of coefficients for
equalizing said more than one carriers without separating said
more than one carriers from the spectrum of said composite signal
15 prior to equalization;

 means (30,38) for deriving an error signal
representing a condition of said PAM signal; and

 means (22) for coupling said error signal to said signal
conditioning means.

20

2. Apparatus according to claim 1, wherein

 said multiple carrier composite signal comprises a first
carrier modulated by a first information component and a second
carrier modulated by a second information component;

25 said deriving means includes means for separating
said first information component and said second information
component of said conditioned composite signal, and detector
means responsive to a separated component from said sensing
means for developing said error signal; and wherein said

30 apparatus further includes

 means for combining said separated first and second
components.

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3. Apparatus according to claim 1, wherein
said equalizer means exhibits non-time-multiplexed
operation.

5

4. Apparatus according to claim 2, wherein
said composite signal is a digital high definition
television signal and said first and second components are
frequency multiplexed in a baseband spectrum.

10

5. Apparatus according to claim 4, wherein
said first and second components exhibit different
carrier frequencies and different bandwidths occupying different
portions of a television signal video spectrum.

15

6. Apparatus according to claim 2, wherein said signal
conditioning means further includes
de-rotator means responsive to an equalized
composite signal from said equalizer means, and to an error signal
developed by said detector means for maintaining a desired
orientation of said constellation.

7. Apparatus according to claim 6, wherein
said detector means derives first and second error
signals from said separated first and second components,
respectively;

said equalizer means is responsive to said first and
second error signals; and
said de-rotator means is responsive to one of said
error signals.

8. Apparatus according to claim 2 and further
comprising
means for differentially decoding said first component
and said second component prior to being combined by said
combining means.

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9. Apparatus according to claim 4, wherein
said baseband spectrum is constituted by a first
frequency band occupying the lowermost portion of said
5 spectrum, and a second frequency band occupying the remainder
of said spectrum, said first band being narrower than said second
band, exhibiting higher energy than said second band, and
containing higher priority information than said second band.
- 10 10. Apparatus according to claim 9, wherein
said first band contains low frequency video
information and audio information; and
said second band contains high frequency video
information occupying frequencies including standard
15 chrominance frequencies and a standard chrominance subcarrier
frequency.
11. Apparatus according to claim 1, wherein
said adaptive equalizer means is a fractionally spaced
20 passband equalizer.
12. In a system for processing a television signal,
digital signal processing apparatus wherein:
input means (10) for receiving a composite multiple
25 carrier PAM signal, said multiple carrier composite signal
comprising a first carrier modulated by a first component, and a
second carrier modulated by a second component;
signal conditioning means (18-26) including adaptive
equalizer means (20) exhibiting non-time-multiplexed operation
30 and responsive to said composite signal for providing an equalized
composite signal at an output, said equalizer means including a
single equalizing device having a response encompassing said first
and second modulated carriers for equalizing said first and second
modulated carriers without separating said first and second
35 modulated carriers from the spectrum of said composite signal
prior to equalization;

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means (32,34) for separating said first component and said second component of a conditioned composite signal from said conditioning means;

first means (28,40) responsive to separated data
5 associated with said first component for producing corresponding output data;

first detector means (30) for producing a first error signal (E1) representing an offset between respectively corresponding input and output data of said first means;

1 0 second means (36,42) responsive to separated data associated with said second component for producing corresponding output data;

second detector means (38) for producing a second error signal (E2) representing an offset between respectively
1 5 corresponding input and output data of said second means;
wherein

said adaptive equalizer means (20) is responsive to said first and second error signals.

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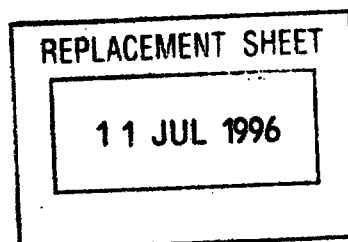
MULTIPLE CARRIER DIGITAL
TELEVISION SIGNAL DECODER

Abstract of the Disclosure

In a video signal processing system, a single adaptive passband equalizer (20) is used to process a composite Quadrature
5 Amplitude Modulated (QAM) signal encoded with high priority (HP) and standard priority (SP) components. The equalizer output is phase corrected by a de-rotator(24), and filtered (32,34) to separate the HP and SP components. Error signals respectively representing HP and SP phase errors are developed (30,38). One
10 of the error signals (E1) controls the operation of the de-rotator. Both error signals are used to generate (22) updated coefficients for the adaptive equalizer. Afterwards the HP and SP components are decoded (40,42) and combined (48).

15

FIGURE 1



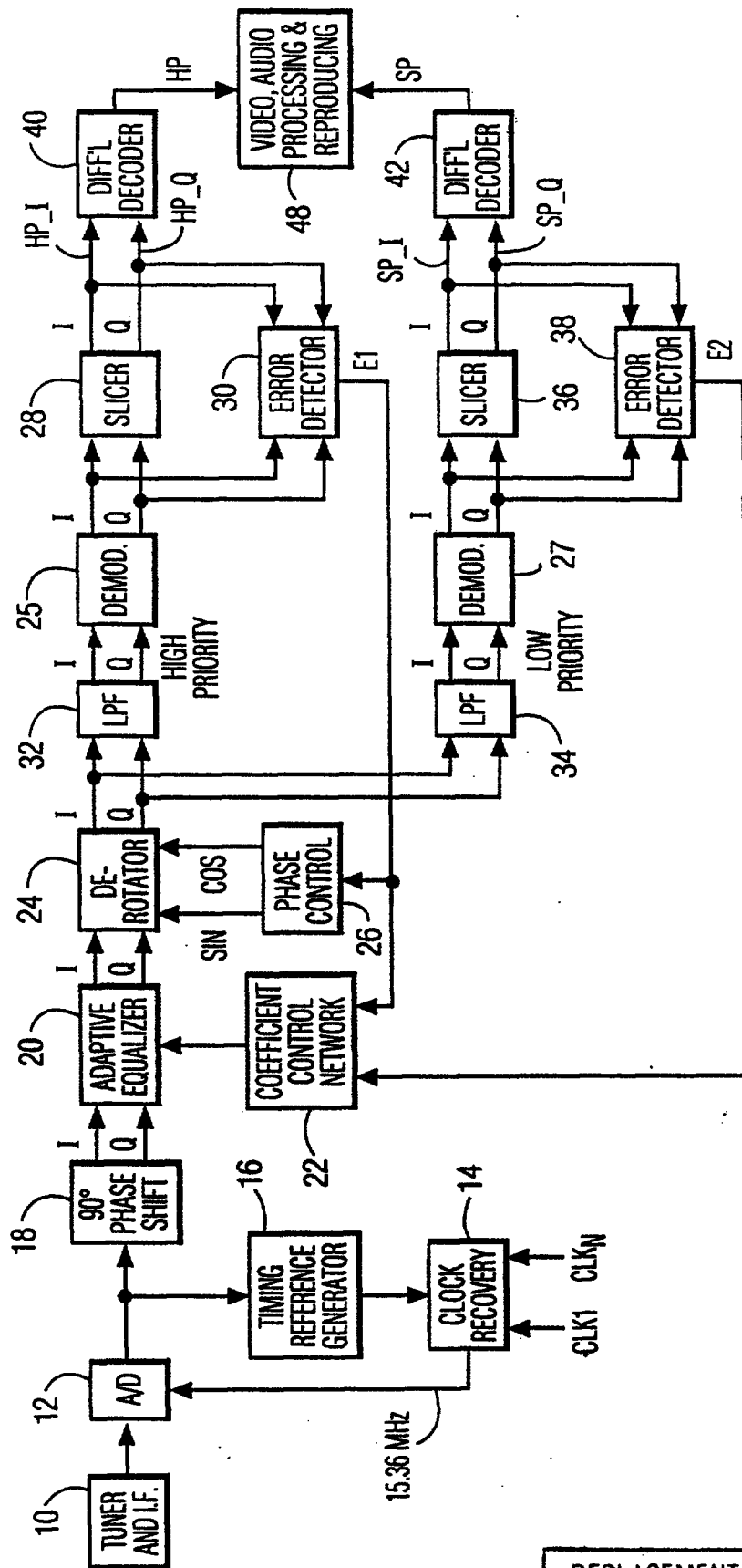


FIG. 1

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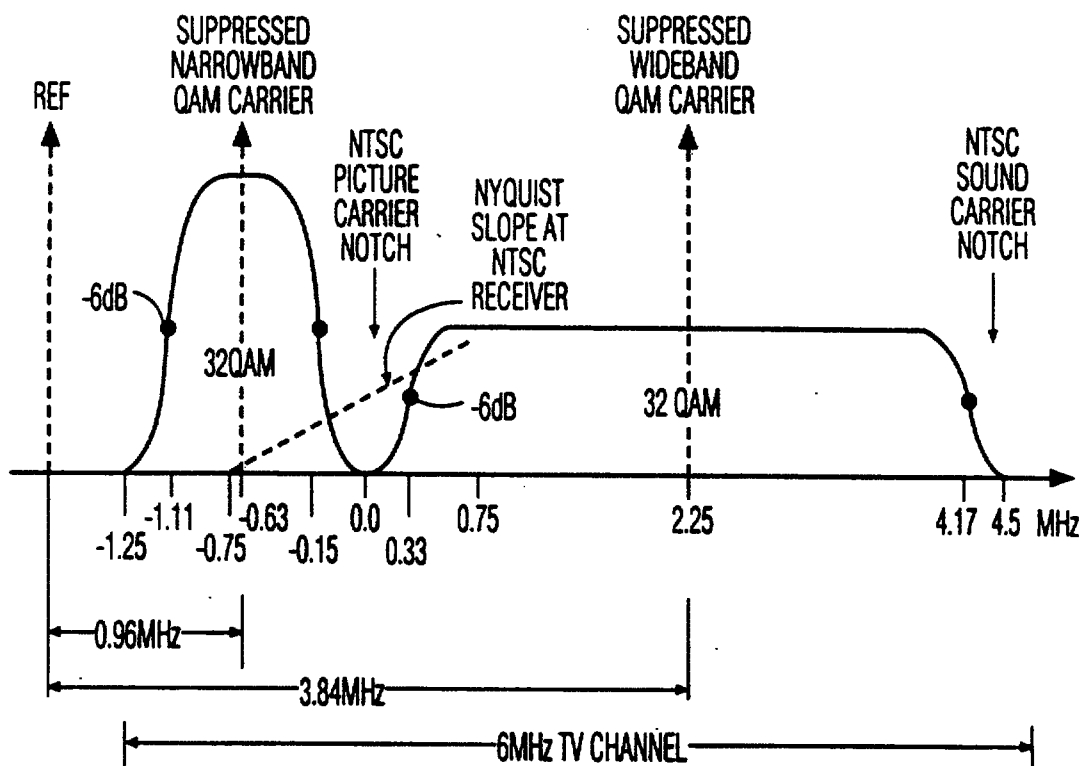


FIG. 2

